Design of Broadband High Gain Polarization Reconfigurable Fabry-Perot Cavity Antenna Using Metasurface

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A broadband high gain polarization reconfigurable antenna based on metasurface has been presented. The antenna is composed of a planar metasurface, a slot antenna and an air cavity. The metasurface is made up of 64 identical patches, and all the patches are on the top surface of the substrate. The spatial equivalent circuit of the metasurface is discussed and two approximate calculation formulas of the equivalent circuit are obtained. The antenna can be reconfigured to linear polarization, left-hand and right-hand circular polarizations by adjusting the relative positions between the metasurface and the planar slot antenna. The gain of the antenna is improved. In order to verify these methods, the antenna is studied and designed to operate at around 11GHz. The simulated and measured results show that the 3dB axis ratio bandwidth is 10–12 GHz (fractional bandwidth 18.18%) and maximum gain of 14.6 dBi.

Keywords: metasurface, polarization reconfiguration, Fabry-Perot cavity, high gain, slot antenna

INTRODUCTION

Metamaterials, such as metasurface (MS), electromagnetic band gap (EBG), photonic band gap (PBG), frequency selective surface (FSS) and left handed metamaterials (LFM), are commonly designed by arranging a number of electrically small scatterers in regular or irregular periods within a space region to obtain some special electromagnetic behaviors [1–5]. In recent years, reconfigurable antennas based on metasurface have been attracting a wide attention of researchers [6–10]. Reconfigurable antennas generally include operating frequency, radiation pattern, and polarization modes tunability, which can well meet the complex communication systems and multitasking demands [11–13]. Polarization reconfigurable antennas are usually able to achieve polarization mode transitions. For example, the antenna can be reconfigured to left-hand circular polarization (LHCP), right-hand circular polarization (RHCP) and linear polarization [14–17]. The direction of the electric field vector is changed at the time of reconstruction. Frequency reconfigurable antennas are very useful owing to their tunable operating frequency, which can be classified into two types, band switching and continuous tuning, respectively [18–21]. The radiation pattern of an antenna can be classified into omnidirectional radiation, bidirectional radiation, unidirectional radiation and multidirectional radiation. Radiation pattern reconfigurable antennas can usually be switched from one radiation pattern to another.
Just as a two-dimensional equivalent of metamaterial, metasurface, which cannot be really found in the nature, is essentially periodic arrangements of scatterers or apertures in order to achieve the characteristics of specialized engineering [22, 23]. Research shows that MS can be used to enhance the performance of antennas. Thus, much research work
FIGURE 3 | Electric field distribution at $f = 11$ GHz for the unit cell of the proposed MS. (A) $\theta = 0^\circ$ and (B) $\theta = 45^\circ$. 
has been carried out in the field of improving antenna gain, achieving polarization reconfigurable and frequency reconfigurable antennas by using MS.

In literature [24], a frequency and polarization reconfigurable antenna consisting of a frequency reconfigurable MS, a polarization reconfigurable MS and a microstrip patch antenna with the same diameter is proposed. The polarization reconfigurable MS consists of periodic corner-truncated square elements placed on the upper surface of the frequency reconfigurable MS, and the microstrip patch antenna placed in the bottom layer as a source antenna. By rotating the frequency reconfiguration MS, the designed antenna has a tuning range of 4.0–4.35 GHz. By rotating the polarizable reconfigurable surface, the designed antenna can realize the transformation of linear and circular polarization at 5.0–5.2 GHz (relative bandwidth 4%). In [25], the studies of polarization reconfigurable antenna with a slot antenna and an asymmetric cross shaped MS are conducted. The linear polarization of the slot antenna is reconfigured into LHCP and RHCP by rotating the MS around the center of the slot antenna. The designed polarization reconfigurable antenna has a 3 dB axis ratio (AR) bandwidth of 4.29–4.41 GHz (relative bandwidth 2.7%). In [22], a radiation pattern reconfigurable antenna based on MS is proposed. The operating frequency range of the designed radiation pattern reconfigurable antenna is 5.4–5.6 GHz. A low profile broadband circularly polarized MS antenna was proposed in [26]. The MS consisting of 4 × 4 square metal patches to realize the miniaturization of the antenna. The 3 dB axial ratio bandwidth is 1.4–1.62 GHz (relative bandwidth 14.5%).

The operating bandwidth of the previously published literature with polarization reconfigurable and radiation pattern reconfigurable antenna is often subject to the restriction of the structure of MS, As is in [26], the 3 dB AR is only 14.5%. In this paper, a polarization reconfigurable antenna using an improved MS is proposed. When the antenna operates in circular polarization, there will be three inflection points in the AR curve. Thus, the 3 dB AR bandwidth is expanded greatly.

In this paper, a reconfigurable antenna using an improved MS is proposed. The 3 dB AR bandwidth is expanded greatly. To clearly show that this antenna can provide circular polarization radiation, the vector electric field at different phases from 0 to 360 degrees, at the antenna aperture in the far field is analyzed. Our work extracts and analyses the equivalent circuit parameters of the improved MS. In the new design, Fabry-Perot cavity antenna and MS are combined to expand the bandwidth of antenna, improve the gain of antenna, and realize polarization reconfiguration.

TOPOLOGY STRUCTURE AND PRINCIPLE OF OPERATION OF THE RECONFIGURABLE POLARIZATION CONVERTER

As is shown in Figure 1, the proposed MS is made up of 64 identical periodic patches, and all the patches are on the top surface of the dielectric substrate. In Figure 1A, the structure within the area enclosed by the red curve can be considered as a unit cell. In order to analyze the polarization properties of the MS, the unit cell is enlarged and redrawn, as is presented in Figure 1B.

The perpendicular E-field components broken down by the MS will cause two different impedances. The expression for two impedances is shown in Equations (1) and (2).

\[
Z_1 = 2R_1 + j\omega(2L_1) + \frac{1}{j\omega C_1} = R_{Z1} + jX_{Z1}
\]

\[
Z_2 = 2R_2 + j\omega(2L_2) + \frac{1}{j\omega C_2} = R_{Z2} + jX_{Z2}
\]

The spatial equivalent circuit of the metal microstrip structure is discussed in literature [27]. The equivalent circuit of the
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Metasurface is analyzed and two approximate calculation formulas of the equivalent circuit are obtained. As is shown in Equations (3) and (4), \( \varepsilon_0 \) is the permittivity and \( \mu_0 \) is the permeability of the free space; \( \varepsilon_r \) is dielectric constant of substrate; \( \gamma_g \) is the relative distance of two patches, which is related to the dimension of the patch and the cutting part; \( \eta \) is length of the truncated patch; \( p \) is the length of the patch; \( b \) is the length of the unit cell.

\[
C = \varepsilon_0 \varepsilon_r \left( \frac{2\sqrt{2}b}{\pi} \ln\left( \frac{1}{\sin\left( \frac{\gamma_g}{2\sqrt{2}b} \right)} \right) \right) \quad (3)
\]

\[
L = \frac{\mu_0}{\sqrt{2\pi}} \frac{b}{\ln\left( \frac{1}{\sin\left( \frac{\eta}{2\sqrt{2}b} \right)} \right)}, \quad \eta = \sqrt{2}b - \gamma_g \quad (4)
\]

According to Equations (3) and (4), when \( \gamma_g \) increases, the \( L_2 \) increases and the \( C_2 \) decreases. Thus, the value of \( X_{Z_2} \) becomes large, making \( Z_2 \) less capacitive than \( Z_1 \). The phase difference between \( Z_1 \) and \( Z_2 \) can be achieved by varying the dimension of the truncated corners. When the unit cell is truncated such that \( |Z_1| = |Z_2| \), and \( \angle Z_2 - \angle Z_1 = 90^\circ \), then \( |E_1| = |E_2| \) and \( \angle \vec{E}_2 - \angle \vec{E}_1 = 90^\circ \). The antenna will be RHCP. As is shown in Figure 2B, when the MS is rotated 45° or 135° in the counterclockwise direction, the antenna is changed to LP. When the rotation angle is 90°, the antenna is reconfigured to LHCP. The schematic assembly of antenna is drawn in Figure 2A. It can be seen that the reconfigurable antenna presented in this paper consists of a slot antenna, a supersurface and an air cavity. These three components together form the Fabry-Perot cavity antenna in structure.

The property of the metasurface layer is highly relevant with the characteristics of the fabry-perot resonator antenna. In addition, the frequency resonance of an fabry-perot resonator antenna can be described as

\[
2n\pi = \frac{4\pi h_0}{c} f + \psi_m + \psi_r, \quad n = 0, 1, 2 \ldots \quad (5)
\]

where \( \psi_m \) and \( \psi_r \), respectively, represent the reflection phases of the metasurface layer and the ground plane, and \( h_0 \) is the height of the fabry-perot cavity. Supposing that the ground plane is perfectly electric conducting (\( \psi_r = -\pi \)) and the reflection

![Image](image_url)

**Figure 6** | Photograph of the designed antenna and Antenna test system. (A) feeder line of slot antenna, (B) surface of slot antenna, (C) surface of MS, (D) antenna measurement setup.
phase of the metasurface layer varies around \(-\pi\), according to equation (5), the fabry-perot cavity has a minimum height \(h\) of \(\sim \lambda/2\) when the fabry-perot resonator antenna operates at the first resonance \((n = 0)\).

As we know, the Fabry-Perot cavity can improve the gain of antenna greatly. In this design, a slot patch antenna which is chosen has the potential of easy feed, stable transverse radiation and wide bandwidth. Complete schematic with the dimensions of feeder line of the source antenna is drawn in Figure 2C. The surface source antenna is drawn in Figure 2D.

To demonstrate the circular polarization (CP) characteristics of MS, the simulated current distribution on the MS antenna at different time points is shown in Figure 3. It is obvious that the electric field vector distribution varies and rotates with time. Numerical simulations have been performed by using the full wave electromagnetic simulator HFSS. Figure 3A shows the direction of rotation of the electric field vector of the metasurface's unit cell when \(\theta = 0^\circ\). According to the rotation direction of the electric field vector, the electric field is RHCP.

Figure 3B shows the direction of the electric field vector when \(\theta = 45^\circ\). According to the direction of the electric field vector, the electric field is LP at this time. The
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simulated reflection and transmission coefficients of the metasurface's unit cell under normal incidence are plotted in Figure 4.

As described above, the size of the $h_0$ is affected by the reflection phase of the metasurface. However, the reflection phase of the metasurface also changes with frequency. The simulation results of reflection phase of the metasurface are shown in Figure 5. According to the size of $h_0$, the phase difference caused by the path difference can be calculated. Figure 5 also shows the path difference $\phi_d$, the reflection phase $\phi_m$ of the metasurface and the total phase difference $\Psi$ at different frequencies. As shown in Figure 5, the total phase difference $\Psi$ is close to 0 at 10.5 GHz when $\theta = 45^\circ$, where the same phase superposition maximizes the gain of the antenna. When $\theta = 0^\circ$, the total phase difference $\Psi$ is close to 0 at 11 GHz. The maximum gain of antenna will appear at 11 GHz. The gain of the antenna will also change with the total phase difference $\Psi$.

**POLARIZATION RECONFIGURABLE ANTENNA BASED ON METASURFACE**

In order to verify the correctness of the antenna design method in the previous section, much research has been carried out and the experimental results show that when the cutting shape is fan-shaped, the bandwidth for circularly polarized has been greatly expanded. Photographs of antennas and test systems are shown in Figure 6.

The antenna is designed on RO4003C substrate with $\varepsilon_r=3.55$, 32 mil thickness. As shown in Figure 5, the optimized dimensions of the antenna are $T = 80$ mm, $h_0 = 16.2$ mm $W_1 = 6$ mm, $L_1 = 6.7$ mm, $W = 1.72$ mm, $L = 38.9$ mm, $W_{s1} = 2.2$ mm, $L_{s1} = 23.5$ mm, $L_s = 41.1$ mm, $p = 7$ mm, $g = 3.42$ mm, $b = 9$ mm. The simulated and measured S11 of the designed antenna with different rotation angles are shown in

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**FIGURE 9** | Measured and simulated radiation patterns and gains with different rotation angle at 11 GHz.
at 11 GHz, when $\theta = 0^\circ$. Figure 10 shows the gain of the slot antenna and the gain of the reorganizable antenna. The gain of slot antenna is about 6–7 dBi. When the MS is placed atop the slot antenna, the gain of the antenna is obviously increased. The value of the gain increases by about 7 dBi on average.

The comparison between our work and some published polarization reconfigurable antennas is illustrated in Table 1. This work shows wider bandwidth and higher gain performance. The design method presented in this paper has proved that MS can be used to improve antenna performance more effectively.

**CONCLUSIONS**

A broadband high gain polarization reconfigurable antenna based on MS has been presented. The antenna is composed of a planar MS and a slot antenna. The proposed antenna can be reconfigured to LHCP, RHCP and LP by adjusting the relative position between the MS and the slot antenna. The antenna is studied and designed to operate at around 11 GHz. The S11, AR, radiation patterns and gain of the antenna are measured. The measured results show that the maximum gain of the proposed antenna is 14.6 dBi and that the 3 dB AR bandwidth is 10–12 GHz with state-of-the-art measured performance.

**DATA AVAILABILITY STATEMENT**

All datasets generated for this study are included in the article/supplementary material.

**AUTHOR CONTRIBUTIONS**

CN developed the concept and supervised the whole project. CL carried out the simulations and designed the structure and fabricated the sample. CN and CL analyzed the simulation data and contributed to writing and finalizing the paper. ZZ and LZ performed the experiments. MC contributed to paper revision and language editing. All authors contributed to the article and approved the submitted version.

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**TABLE 1** Comparison of some published polarization reconfigurable antennas and our work.

| $f_0$ (GHz) | 3 dB AR Bandwidth (%) | Peak gain (dBi) | Polarization |
|-------------|------------------------|-----------------|-------------|
| Kandasamy et al. [25] | 4.35 | 2.7 | 6.5 | LP/LHCP/RHCP |
| Liu et al. [26] | 1.51 | 14.5 | 7 | RHCP |
| Fan et al. [28] | 10 | 16 | 17.9 | LHCP |
| Li et al. [29] | 8.9 | 13.8 | 11.2 | LHCP |
| Hu et al. [30] | 5.5 | 17.8 | 9.39 | LP/LHCP/RHCP |
| Zhu et al. [31] | 3.5 | 11.4 | 7.5 | LP/LHCP/RHCP |
| This work | 11 | 18.18 | 14.6 | LP/LHCP/RHCP |

**Figure 7.** The measured results are in good agreement with the simulated results.

The simulated and measured AR of the designed antenna with different rotation angle $\theta$ is shown in Figure 8. The measured 3 dB AR bandwidth is 10–12 GHz (relative bandwidth 18.18%) for the rotation angle $\theta = 0^\circ$ and $\theta = 90^\circ$. The simulated and measured radiation patterns and gains of the proposed antenna at 11 GHz are illustrated in Figure 9. The measurements of the antenna pattern are only performed around the main beam for achieving more accurate test results. The measured maximum gain of the designed antenna is more than 14 dBi, when $\theta = 0^\circ$, $\theta = 45^\circ$, $\theta = 90^\circ$, and $\theta = 135^\circ$. The maximum peak is 14.6 dBi.
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Conflict of Interest: The authors declare that the research was conducted in the absence of any commercial or financial relationships that could be construed as a potential conflict of interest.

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