Design of a Compact 5.7–5.9 GHz Filter Based on CRLH Resonator Units

Shanwen Hu*, Yiting Gao, Xinlei Zhang, and Bo Zhou

Abstract—A compact substrate integrated waveguide (SIW) filter based on composite right/left-handed (CRLH) resonator units is implemented in this paper. The filter is composed of two CRLH resonator units serially connected by a SIW transmission line unit. The structure of the filter and equivalent circuit transmission behavior are analyzed, and a novel design method by optimizing the length and width of the interdigital metal slots to decrease the filter operation frequency is proposed. To further demonstrate the design theory and performance of the proposed filter, the filter was designed and fabricated on an RT6010 dielectric material. The measurement results show that the proposed filter works at a center frequency of 5.8 GHz with 200 MHz bandwidth. The insertion loss is 2.3 dB, and the filter size is only 10 mm × 7.4 mm.

1. INTRODUCTION

RF filter is one of the key components for modern wireless communication systems to select the passband signal and reject the stopband signal. Most commercial communication standards are focused on the frequency band that lower than 6 GHz, such as LTE, 5G, Wi-Fi, Bluetooth, and Zigbee. Hence, the design of compact sub-6G filters is a hot research topic for mobile portable devices. Substrate integrated waveguide (SIW) is widely used in RF passive device designs due to low loss, low cost, and flexibility of integration properties, such as filter [1–6], antenna [7–11], phase shifter [12–16], power divider [17–21], and coupler [22–26]. However, SIW filters under 6 GHz are still outsize to meet the requirement of portable communication devices because of the long wavelength. Numerous research works have been presented to reduce size of SIW filters. Due to the advantage of zero order resonance characteristic which makes its resonance frequency relatively irrelevant with device size [27], a CRLH structure is proposed and studied to minimize the size of SIW passive devices [28–33]. A typical rectangular CRLH filter is reported in [30] with compact size, and the operation frequency is 6.8 GHz with 3 dB insertion loss, which is still out of 6 GHz frequency limitation. In this work, a novel design method is proposed to further realize a compact CRLH filter working inside 6 GHz frequency range. The structure and equivalent circuit are analyzed to discuss the frequency limitation of the filter. The coupling capacitor of the filter is then designed and optimized to reduce resonate frequency. A 5.8 GHz RF filter with 200 MHz bandwidth is finally implemented for sub-6G wireless systems with a size of only 10 mm × 7.4 mm, and the insertion loss is low as 2.3 dB.

2. FILTER STRUCTURE AND ANALYSIS

The designed SIW filter based on CRLH resonator units is shown in Fig. 1(a). Two CRLH resonators composed of interdigital rectangular-shaped metal slots are coupled with a SIW transmission line (SIW
Metallization through holes are placed as vias to connect CRLH units to backside ground. The SIW TL is adopted to restrict the propagating waves by arrays of vias which results in low loss for the filter. The CRLH units can demonstrate resonators which are independent of their physical lengths, and hence they can be more compact, especially at lower frequencies.

The equivalent circuit of single CRLH resonator unit is shown in Fig. 1(b). The filter circuit is composed of a left-hand series capacitor $C_L$, a shunt inductor $L_L$, a right-hand shunt capacitor $C_R$, and a series inductor $L_R$. Capacitor $C_L$ is the coupling capacitor between the interdigital fingers of the CRLH units, and $C_R$ is the coupling capacitor from the finger slots to the ground. Inductor $L_L$ is introduced by the self-inductance of the vias in the structure, and $L_R$ is generated by the inductance of the rectangular slots in the CRLH units. The “left-hand” property is under a certain frequency range when electromagnetic wave passes through the structure, and the effective dielectric constant and effective permeability are negative. On the other hand, the “right hand” property is under another frequency range, and the effective dielectric constant and effective permeability are positive. Therefore, complex resonance behavior of this structure can be accomplished to improve the performance of RF passive devices.

![Figure 1. (a) Conventional SIW filter with interdigital rectangular CRLH units, (b) equivalent circuit of single CRLH resonator unit.](image1)

The proposed filter is composed of two CRLH resonator units which are connected with the SIW TL. The overall equivalent circuit of the filter is illustrated in Fig. 2. In the equivalent circuit, $R_1$, $R_2$, and $R_3$ are the series and shunt resistances of the lossy material. $C_1$ and $C_2$ are generated by the right-handed capacitances ($C_R$) of two CRLH units, while $C_3$ is generated by the left-handed capacitance ($C_L$) of two CRLH units. Consequently, $C_1$ and $C_2$ are determined by the area of rectangular plates of CRLH units, and $C_3$ is determined by the length of interdigital slots of CRLH units.

![Figure 2. The equivalent circuit of the filter.](image2)

A simplified equivalent Y model is illustrated in Fig. 3 to calculate the transmission behavior of the filter.

![Figure 3. Simplified Y model of the filter.](image3)
The values of \( R_1, R_2, \) and \( R_3 \) are normally very small which mainly affect the insertion loss, while showing little effect on the resonate frequency, hence these resistances can be neglected in the equivalent circuit. It can be derived from the equivalent circuit in Fig. 2 and Fig. 3:

\[
Y_1 = \frac{1 - \omega^2 L_1 C_1}{j \omega L_1} \\
Y_2 = \frac{1 - \omega^2 L_2 C_2}{j \omega L_2} \\
Y_3 = \frac{j \omega C_3}{1 - \omega^2 L_3 C_3}
\]

A \( Y \) matrix equation can be derived based on the \( Y \) model in Fig. 3.

\[
\begin{bmatrix}
Y_{11} & Y_{21} \\
Y_{12} & Y_{22}
\end{bmatrix}
= \begin{bmatrix}
Y_1 + Y_3 & -Y_3 \\
-Y_3 & Y_2 + Y_3
\end{bmatrix}
\]

Putting Equations (1)–(3) to the matrix in Equation (4), then

\[
Y_{11} = \frac{1 - \omega^2 L_1 C_1 - \omega^2 L_3 C_3 - \omega^2 L_1 C_3 + \omega^4 L_1 C_1 L_3 C_3}{j \omega L_1 (1 - \omega^2 L_3 C_3)}
\]

(5)

\[
Y_{22} = \frac{1 - \omega^2 L_2 C_2 - \omega^2 L_3 C_3 - \omega^2 L_2 C_3 + \omega^4 L_2 C_2 L_3 C_3}{j \omega L_2 (1 - \omega^2 L_3 C_3)}
\]

(6)

\[
Y_{21} = Y_{12} = \frac{j \omega L_3}{1 - \omega^2 L_3 C_3}
\]

(7)

When the value of \( Y_{21} \) is infinite, or \( Y_{11}/Y_{22} \) equals zero, the circuit will generate resonance. In Equations (5)–(7), the capacitance is normally at pF level, the inductance normally at nH level, and the frequency at GHz level. Consequently, the product term \( \omega^4 L_1 C_1 L_3 C_3 \) and \( \omega^4 L_2 C_2 L_3 C_3 \) in above equations can be neglected. Therefore, three resonant frequencies can be derived:

\[
f_{O1} = \frac{1}{2 \pi \sqrt{L_3 C_3}}
\]

(8)

\[
f_{O2} = \frac{1}{2 \pi \sqrt{L_1 C_1 + L_3 C_3 + L_1 C_3}}
\]

(9)

\[
f_{O3} = \frac{1}{2 \pi \sqrt{L_2 C_2 + L_3 C_3 + L_2 C_3}}
\]

(10)

It is illustrated in Equations (8)–(10) that three resonant frequencies are generated by this CRLH structure, and the value of the resonant frequency is dominated by capacitances and inductances. The inductances are obtained solely by the metallic vias between the plates, which are fixed in the design. Consequently, the capacitances provided by interdigital capacitance and ground-coupling capacitance become the only alterable elements. Therefore, a novel design method is proposed in this work by optimizing length \( L_1 \) to increase \( C_3 \) and width \( W_1 \) to increase \( C_1 \) and \( C_2 \), which will be discussed in details in the following section.

If the SIW TL section (as shown in Fig. 1(a)) is taken into account, then the total phase shift of the CRLH filter on achieving a zeroth order mode can be written as [30]:

\[
\beta l = 2 \phi_C + \phi_{SIW} = 0
\]

(11)

where \( \phi_C \) is the phase shift due to two CRLH units, and \( \phi_{SIW} \) is the phase shift due to the SIW section:

\[
\phi_C = \sqrt{\frac{L_R C_R}{\omega}} - \frac{1}{\omega \sqrt{L_L C_L}}
\]

(12)

\[
\phi_{SIW} = \frac{2 \pi}{\lambda_g} = \frac{2 \pi}{\lambda_0} \sqrt{1 - \left(\frac{\lambda_0}{2 a_{eff}}\right)^2}
\]

(13)
where \( a_{\text{eff}} \) is the effective width of the SIW TL, then a resonant frequency can be derived by putting Equations (12) and (13) to Equation (11) and solving the equation:

\[
\omega = \frac{\pi}{\lambda_0} \sqrt{\frac{1 - \left( \frac{\lambda_0}{2a_{\text{eff}}} \right)^2}{\left( \frac{\pi}{\lambda_0} \right)^2 \left[ 1 - \left( \frac{\lambda_0}{2a_{\text{eff}}} \right)^2 \right] + \frac{4\sqrt{L_RC_R}}{\sqrt{L_CL_L}}}}
\]

(14)

It is shown in Equation (14) that the SIW TL section gives us more freedom to tune the operation frequency of the CRLH filter by optimizing the effective width of the SIW TL section \( (a_{\text{eff}}) \). Consequently, the CRLH filter with SIW TL section shows the potential to achieve a compact size.

3. FILTER DESIGN

Based on above analysis, the resonant frequencies of the filter are determined by the series interdigital capacitance \( C_3 \) and the shunt ground-coupling capacitance \( C_1/C_2 \). The value of \( C_3 \) depends on the length of the interdigital metal slots \( (L_1) \), and the value of \( C_1/C_2 \) depends on the width of the interdigital metal slots \( (W_1) \).

An AWR design environment software is used to simulate this filter. The equivalent circuit elements can be derived by generating a special model, which is achieved by simulating the frequency response of the filter using the AWR software. In this work, the value of \( C_3 \) varying with different length \( L_1 \) is simulated while keeping other dimension parameters constant, which is shown in Fig. 4. It is illustrated that the average value of \( C_3 \) is only 3.5 pF when \( L_1 = 2 \) mm. The value increases to 12 pF when \( L_1 = 5 \) mm, and the resonant frequencies are then decreased according to Equations (8)–(10). For the trade-off among resonant frequency, filter size, insertion loss, and matching performance, the final value of length \( L_1 \) is chosen as 4 mm.

The values of \( C_1/C_2 \) varying with different lengths \( W_1 \) are also simulated while keeping other dimension parameters constant, shown in Fig. 5. The curves of \( C_1 \) and \( C_2 \) coincide with each other in Fig. 5 due to the same value of \( C_1 \) and \( C_2 \) as a result of the symmetrical structure. It is illustrated that the average value of \( C_1/C_2 \) is only 1.2 pF when \( L_1 = 0.2 \) mm. The value increases to 4.9 pF when \( W_1 = 0.8 \) mm, and the resonant frequencies are then decreased according to Equations (9)–(10). For the trade-off among resonant frequency, filter size, insertion loss, and matching performance, the final value of width \( W_1 \) is chosen as 0.6 mm.

The bandwidth of the filter can be realized by tuning the equivalent inductance and capacitance values of the structure. The two CLRH units as shown in Fig. 1 are usually symmetrical, so \( L_1 \) is the
same as $L_2$, and $C_1$ is the same as $C_2$. Therefore, the resonant frequency $f_{o2}$ equals $f_{o3}$ in Equations (9)–(10). It can be easily observed in Equations (8)–(10) that the resonant frequency $f_{o1}$ is higher than $f_{o2}$ or $f_{o3}$. The equivalent elements $L_3$, $C_3$ can be firstly optimized to set $f_{o1}$ as 5.9 GHz. Then $L_1$, $C_1$, $L_2$, $C_2$ can be further tuned to set $f_{o2}/f_{o3}$ as 5.7 GHz. Consequently, 200 MHz bandwidth is finally realized.

For the design of the proposed filter, the insertion loss, stopband rejection, and matching properties are also considered as critical design factors to tune the filter parameters except resonant frequency. The final physical parameters after optimization are shown in Table 1. A compact SIW filter is then finally designed and optimized. The simulated $S$ parameters are shown in Fig. 6. The center resonant frequency is 5.9 GHz with 200 MHz bandwidth. This center frequency is 100 MHz higher than the 5.8 GHz design goal, since the measured center frequency will normally decrease to the lower frequency after fabrication. The insertion loss is only 1.93 dB. Consequently, a compact filter with low resonant frequency and low loss is successfully designed based on the optimization method proposed in this work. With these properties, the proposed filter shows the potential ability to be used in sub-6G wireless communication systems.

Table 1. Dimensions of the proposed filter.

| Dimension | Value (mm) | Dimension | Value (mm) |
|-----------|------------|-----------|------------|
| $W_1$     | 0.6        | $L_1$     | 4          |
| $W_2$     | 10         | $L_2$     | 7.4        |
| $W_3$     | 0.2        | $L_3$     | 1.1        |
| $W_4$     | 1          | $L_4$     | 5.8        |
| $W_5$     | 0.5        | $L_5$     | 0.7        |
| $W_6$     | 5          | $W_7$     | 4.6        |

Figure 6. Simulated $S$ parameters of the filter.

4. IMPLEMENT AND MEASUREMENT

To further demonstrate the merit, a SIW filter based on the proposed interdigital CRLH units is implemented with RT6010 material of which dielectric constant is 10.2, as shown in Fig. 7. The core filter size is only 10 mm × 7.4 mm.

The input and output signals are fed in and out through the RF SMA connectors. The $S$ parameters measurement results are shown in Fig. 8. It shows that the working frequency band of this proposed filter ranges from 5.7 GHz to 5.9 GHz, and the insertion loss $S_{21}$ is only 2.3 dB. The measured group delay of the proposed filter is shown in Fig. 9. The maximum passband group delay is located at
Figure 7. Photo of the filter, (a) topside, (b) backside.

Figure 8. Measured $S$ parameters of the filter.

Figure 9. Measured group delay of the filter.

5.73 GHz, which is 2.85 ns. The minimum passband group delay is 2.08 ns at 5.8 GHz. Therefore, the group delay variation during the whole passband is only 0.77 ns, which is low for this 200 MHz compact filter. Hence, a novel compact CRLH SIW filter is successfully designed and implemented for sub-6G applications. The measurement results demonstrate that the designed method proposed in this work can effectively decrease the operation frequency of a CRLH filter to meet the requirement of sub-6G applications, while maintaining compact size, low loss, and low group delay properties of the filter.

Many studies have been focused on improving the performance of the compact CRLH filter in recent years. The performances of several reported CRLH filters are summarized and compared in Table 2. The physical sizes of the reported filters are normalized by the wavelength of the center frequency ($\lambda_0$). The operation frequency of the filter, reported in [29], can be as low as 3 GHz, with a good bandwidth. However, the size of this filter is too large ($0.8\lambda_0 \times 0.5\lambda_0$). In [30, 31], two relatively compact filters using

| Ref.  | Center frequency (GHz) | Insertion loss (dB) | Bandwidth (MHz) | Size ($\lambda_0 \times \lambda_0$) |
|-------|------------------------|---------------------|-----------------|---------------------------------|
| [29]  | 3/6/9                  | 3                   | 150/500/300     | 0.8 $\times$ 0.5                |
| [30]  | 6.8                    | 3                   | 200             | 0.23 $\times$ 0.14              |
| [31]  | 7.3                    | 2.2                 | 50              | 0.40 $\times$ 0.32              |
| [32]  | 5.3                    | 2.7                 | 500             | 0.51 $\times$ 0.13              |
| [33]  | 5                      | 2.7                 | 700             | 0.37 $\times$ 0.25              |
| This work | 5.8                | 2.3                   | 200             | 0.19 $\times$ 0.14              |
CRLH units are reported. However, their center operation frequencies are beyond the 6 GHz limitation. Two CRLH filters, presented in [32, 33], are well designed for sub-6G applications. However, their sizes are still large to meet the requirement of portable devices. For the design proposed in this work, the filter size is only 0.19λ₀ × 0.14λ₀, and the center frequency is only 5.8 GHz. It is demonstrated that the proposed filter can be considered as one of the most compact CRLH filters with a low passband loss and high stopband rejection for sub-6G systems.

5. CONCLUSION

A novel SIW filter with CRLH resonator units is designed for sub-6G communication systems. The structures of the resonator units and filter are discussed. The key factors to limit the resonant frequencies are calculated and analyzed. A novel design method is proposed by optimizing length \( L_1 \) to increase interdigital capacitance \( C_3 \) and width \( W_1 \) to increase ground-coupling capacitance \( C_1 \) and \( C_2 \). The proposed filter is finally designed, fabricated, and tested, and a 5.7 GHz ~ 5.9 GHz compact filter with only 2.3 dB insertion loss and 0.77 ns group delay variation is successfully realized for sub-6G portable devices.

ACKNOWLEDGMENT

This work was financially supported by the National Natural Science Foundation of China (61501261 & 61504061 & 61504065 & 61601239 & 61704019), the Chinese Postdoctoral Science Foundation (2017M621793 & 2016M601858), and the Natural Science Foundation of Jiangsu (BK20150848 & BK20160906).

REFERENCES

1. Zhu, T., H. Deng, J. Ding, et al., “Compact inline dual-band dual-mode BPF with a hybrid structure of single-layered SIW and CPW,” *IEICE Electronics Express*, Vol. 13, 20160209, 2016.
2. Jia, D., Q. Feng, Q. Xiang, et al., “Multilayer substrate integrated waveguide (SIW) filters with higher-order mode suppression,” *IEEE Microwave and Wireless Components Letters*, Vol. 26, No. 9, 678–680, 2016.
3. Li, P., H. Chu, D. Zhao, et al., “Compact dual-band balanced SIW bandpass filter with improved common-mode suppression,” *IEEE Microwave and Wireless Components Letters*, Vol. 27, No. 4, 347–349, 2017.
4. Lovato, R. and X. Gong. “A third-order SIW integrated filter/antenna using two resonant cavities,” *IEEE Antennas and Wireless Propagation Letters*, 1–1, 2018.
5. Zhang, H., W. Kang, and W. Wu, “Miniaturized dual-band SIW filters using E-shaped slotlines with controllable center frequencies,” *IEEE Microwave and Wireless Components Letters*, 1–3, 2018.
6. Wei, F., X. Y. Wang, Y. K. Hong, et al., “Wideband bandpass filter using U-slotted SW-HMSIW cavities,” *International Journal of RF and Microwave Computer-Aided Engineering*, Vol. 28, No. 2, 1–7, 2018.
7. Saghati, A. P., A. P. Saghati, and K. Entesari, “Ultra-miniature SIW cavity resonators and filters,” *IEEE Transactions on Microwave Theory and Techniques*, Vol. 63, No. 12, 4329–4340, 2015.
8. Sun, L., B. Sun, J. P. Yuan, et al., “Low profile, quasi-omnidirectional, substrate integrated waveguide (SIW) multi-horn antenna,” *IEEE Antennas and Wireless Propagation Letters*, Vol. 15, 1–1, 2015.
9. Martinezros, A. J., J. L. Gomeztonero, and G. Goussetis, “Multifunctional angular bandpass filter SIW leaky-wave antenna,” *IEEE Antennas and Wireless Propagation Letters*, Vol. PP, No. 99, 1–1, 2017.
10. Yu, T., H. Zhao, Z. Li, et al., “Design of planar matching loads for traveling-wave-fed SIW slot arrays,” *IEICE Electronics Express*, Vol. 14, No. 15, 20170467, 2017.
11. Jin, H., Q. Guo, W. Wang, et al., “Integration design of millimeter-wave filtering patch antenna array with SIW four-way anti-phase filtering power divide,” *IEEE Access*, Vol. 7, 49804–49812, 2019.
12. Ebrahimpouri, M., S. Nikmehr, and A. Pourziad, “Broadband compact SIW phase shifter using omega particles,” *IEEE Microwave and Wireless Components Letters*, Vol. 24, No. 11, 748–750, 2014.
13. Ghaffar, F. A. and A. Shamim, “A partially magnetized ferrite LTCC based SIW phase shifter for phased array applications,” *IEEE Transactions on Magnetics*, Vol. 51, No. 6, 1–1, 2015.
14. Muneer, B., Z. Qi, and X. Shanjia, “A broadband tunable multilayer substrate integrated waveguide phase shifter,” *IEEE Microwave and Wireless Components Letters*, Vol. 25, No. 4, 220–222, 2015.
15. Nafe, A. and A. Shamim, “An integrable SIW phase shifter in a partially magnetized ferrite LTCC package,” *IEEE Transactions on Microwave Theory and Techniques*, Vol. 63, No. 7, 2264–2274, 2015.
16. Peng, H., P. Jiang, T. Yang, et al., “Continuously tunable SIW phase shifter based on the buried varactors,” *IEICE Electronics Express*, Vol. 12, No. 7, 20150165, 2015.
17. Djerafi, T., D. Hammou, K. Wu, et al., “Ring-shaped substrate integrated waveguide Wilkinson power dividers/combiners,” *IEEE Transactions on Components, Packaging and Manufacturing Technology*, Vol. 4, No. 9, 1461–1469, 2014.
18. Khan A. A. and M. K. Mandal, “Miniaturized substrate integrated waveguide (SIW) power dividers,” *IEEE Microwave and Wireless Components Letters*, 1–3, 2016.
19. Danaeian, M., A. R. Moznebi, K. Afroz, et al., “Miniaturised equal/unequal SIW power divider with bandpass response loaded by CSRRs,” *Electronics Letters*, Vol. 52, No. 22, 1864–1866, 2016.
20. Yang, Z., W. Chen, H. Lin, et al., “A novel SIW power divider with good out-of-band rejection and isolation.” *IEICE Electronics Express*, Vol. 13, No. 8, 20160160, 2016.
21. Huang, Y. M., W. Jiang, H. Jin, et al., “Substrate-integrated waveguide power combiner/divider incorporating absorbing material,” *IEEE Microwave and Wireless Components Letters*, Vol. PP, No. 99, 1–3, 2017.
22. Jin, H., Z. Zhu, and R. Cheng, “Novel broadband coupler based on corrugated half mode substrate integrated waveguide,” *IEICE Electronics Express*, Vol. 12, No. 24, 20150896, 2015.
23. Qin, J., Y. Zhou, Y. M. Huang, et al., “Miniaturized broadband coupler made of slow-wave half-mode substrate integrated waveguide,” *IEEE Microwave and Wireless Components Letters*, Vol. 27, No. 2, 132–134, 2017.
24. Liu, Z. and G. Xiao, “Design of SIW-based multi-aperture couplers using ray tracing method,” *IEEE Transactions on Components, Packaging and Manufacturing Technology*, Vol. 7, No. 1, 106–113, 2017.
25. Lian, J. W., Y. L. Ban, J. Q. Zhu, et al., “Compact 2-D scanning multibeam array utilizing SIW three-way couplers at 28 GHz,” *IEEE Antennas and Wireless Propagation Letters*, 1–1, 2018.
26. Hageh, M. F., R. Zhang, and D. Peroulis, “High-performance tunable narrowband SIW cavity-based quadrature hybrid coupler,” *IEEE Microwave and Wireless Components Letters*, 1–3, 2018.
27. Lee, J. G. and J. H. Lee, “Zeroth order resonance loop antenna,” *IEEE Transactions on Antennas and Propagation*, Vol. 55, No. 3, 994–997, 2007.
28. Feng, W., Y. W. Qiu, W. S. Xiao, et al., “Compact UWB bandpass filter with dual notched bands based on SCRLH resonator,” *IEEE Microwave and Wireless Components Letters*, Vol. 21, No. 1, 28–30, 2011.
29. Mohan, M. P., A. Alphones, and M. F. Karim, “Triple band filter based on double periodic CRLH resonator,” *IEEE Microwave and Wireless Components Letters*, Vol. 28, No. 3, 212–214, 2018.
30. Abdalla M. A. and K. S. Mahmoud, “A compact SIW metamaterial coupled gap zeroth order bandpass filter with two transmission zeros,” *IEEE International Congress on Advanced Electromagnetic Materials in Microwaves & Optics*, IEEE, 2016.
31. Ahmed, F. D., T. H. Omar, and A. A. Mahmoud, “Ultra compact quad band resonator based on novel D-CRLH configuration,” *IEEE International Symposium on Antennas and Propagation,*
IEEE, 2017.

32. Yang, T., P. L. Chi, R. M. Xu, et al., “Folded substrate integrated waveguide based composite right/left-handed transmission line and its application to partial-plane filters,” *IEEE Transactions on Microwave Theory and Techniques*, Vol. 61, No. 2, 789–799, 2013.

33. Karim, M. F., L. C. Ong, B. Luo, et al., “A compact SIW bandpass filter based on modified CRLH,” *2012 Asia Pacific Microwave Conference Proceedings*, IEEE, 2012.