Output feedback nonlinear control of three-phase grid-connected PV generator

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ABSTRACT
This paper addresses the problem of controlling three-phase grid connected PV system involving a PV arrays, a voltage source inverter, a grid filter and an electric grid. This paper presents three main control objectives: i) ensuring the Maximum power point tracking (MPPT) in the side of PV panels, ii) guaranteeing a power factor unit in the side of the grid, iii) and ensuring the asymptotic stability of the closed loop system. Interestingly, the present study features the achievement of the above energetic goal without resorting to sensors of currents of the grid. To this end, an output-feedback control strategy combining a state observer and a nonlinear control laws is developed. The proposed output-feedback control strategy is backed by a formal analysis showing that all control objectives are actually achieved.

Keywords:
MPPT
Nonlinear control
Nonlinear observer
Output feedback control
Renewable energy
Stability analysis

1. INTRODUCTION
It was very clear from recent studies and documentation that fossil fuels would last only a few more decades. The cost of fossil fuels has become a major challenge for all of humanity. Not only the economic value but also the environmental impacts of fossil fuels have clearly pushed us towards alternatives. The biggest alternatives that can really make a difference to sustainability, such as reducing greenhouse gas emissions and the long-term economy, are renewable energy sources (RES) such as wind and solar energy [1], [2]. PV system is increasing as a renewable source due to its advantages of little maintenance, absence of moving mechanical parts, no noise and no pollutant emission [3]. Furthermore, its cost is decreasing over the next ten years, while the deployment of PV systems continues to increase rapidly. With increasing PV penetration on the grid, eventually reaching hundreds of gigawatts (GW) of interconnected capacity, a variety of methods must be considered and implemented at different scales for a reliable and cost-effective connection into power grid.

Different control strategy for three-phase grid connected of PV modules has been largely dealt with in the specialist literature in the last few years [4]-[9]. Nevertheless, good integration of medium or large PV system in the grid may therefore require additional functionality from the inverter, such as control of reactive power. Moreover, the increase in the average size of a PV system may lead to new strategies such as eliminating the DC-DC converter, which is usually placed between the PV generator and inverter, and moving the MPPT to the inverter, which leads to increased simplicity, overall efficiency and a cost reduction. These two features are present in the three-phase inverter that is presented in this paper, with the addition of a Perturb and Observe (P&O) MPPT algorithm.

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The present paper is then focusing on the problem of controlling three phase grid-connected PV power generation systems. The control objectives are threefold: (i) global asymptotic stability of the whole closed-loop control system; (ii) achievement of the MPPT for the PV array; and (iii) ensuring a grid connection with unity Power Factor (PF). These objectives should be achieved in spite the climatic variables (temperature and radiation) changes. To this end, a nonlinear controller is developed using Lyapunov design technique. A theoretical analysis is developed to show that the controller actually meets its objectives a fact that is confirmed by simulation.

The paper is organized as follows: the three-phase grid connected PV system is described and modeled in Section 2. Section 3 is devoted to controller design and analysis. The controller tracking performances are illustrated by numerical simulation in Section 4.

2. RESEARCH METHOD

2.1. System overview

The main circuit of three-phase grid-connected photovoltaic system as shown in Figure 1. It consists of a PV arrays; a DC link capacitor $C$; a three phase inverter (including six power semiconductors) that is based upon to ensure a DC-AC power conversion and unity power factor; an inductor filter $L$ with a series resistance $r$, and an electric grid. The control inputs of the system are a PWM signals $u_a$, $u_b$, and $u_c$ taking values in the set \{0,1\}. The grid voltages $v_{ga}$, $v_{gb}$ and $v_{gc}$ constitute a three-phase balanced system.

2.2. PV Array model

An equivalent circuit for a PV cell as shown in Figure 2. Its current characteristic can be found in many places [10]-[13] and presents the following expression.

$$I = I_{ph} - I_{sat} \left[ \exp \left( \frac{q(V + IR)}{AKT} \right) - 1 \right] - \frac{V + IR}{R_{sh}}$$  \hspace{1cm} (1)

Where

$$\begin{align*}
I_{sat} &= I_{sat} \left[ \frac{T}{T_s} \right]^3 \exp \left[ \frac{qE_G}{AK} \left( \frac{1}{T_s} - \frac{1}{T} \right) \right] \\
I_{ph} &= \left[ I_{ph} + K_r(T - 298) \right] \lambda
\end{align*}$$  \hspace{1cm} (2)

The meaning and typical values of the parameters given by (1) and (2) can be found in many places (see e.g. [14], [15], [16]). $A$ is diode ideal factor, $k$ is Boltzmann constant, $T$ is temperature on absolute scale in $K$, $q$ is electron charge and $\lambda$ is the radiation in kW/m$^2$, $I_{ph}$ is the short-circuit current at 298 K and 1 kW/m$^2$, $K_r = 0.0017A/K$ is the current temperature coefficient at $I_{ph}$, $E_G$ is the band gap for silicon, is reference temperature, $I_{sat}$ is cell saturation current at $T_s$. PV array consists of $N_i$ cells in series formed the panel and of $N_p$ panels in parallel according to the rated power required. The output voltage and current can be given by the following (3) and (4).
\[ V_{pv} = N_s(V_d - R_s I) \]  
\[ I_{pv} = N_p I \]

Figure 2. Solar cell circuit diagram

The photovoltaic generator considered in this paper consists of several NU-183E1 modules. The corresponding electrical characteristics of PV modules are shown in Table 1. The associated power-voltage (P-V) characteristics under changing climatic conditions (temperature and radiation) are shown in Figures 3 and 4. This highlights the Maximum Power Point (MPP) M1 to M5, whose coordinates are given in Table 3. The data in Table 1 to Table 3 will be used for simulation.

Table 2 shows the main characteristics of the PV array, designed using Sharp NU-183E1 modules connected in a proper series-parallel, making up a peak installed power of 71 kW. As there is no DC-DC converter between the PV generator and the inverter, the PV array configuration should be chosen such that the output voltage of the photovoltaic generator is adapted to the requirements of the inverter. In this case a 380V grid has been chosen, so the inverter would need at least 570V DC bus in order to be able to operate correctly. The minimum number of modules connected in series should be determined by the value of the minimum DC bus voltage and the worst-case climatic conditions. The PV array was found to require 28 series connected modules per string.

Table 1. Electrical specifications for the solar module NU-183E1

| Parameter            | Symbol | Value |
|----------------------|--------|-------|
| Maximum Power        | Pm     | 183W  |
| Short circuit current| Isc    | 8.48A |
| Open circuit voltage | Voc    | 30.1V |
| Maximum power voltage| Vm    | 23.9V |
| Maximum power current| Im    | 7.66A |
| Number of parallel modules| Np | 1     |
| Number of series modules| Ns | 48    |

Figure 3. (P-V) characteristics of The PV Generator (NP=14 And NS=28) with constant temperature and varying radiation

Figure 4. (P-V) characteristics of The PV Generator (NP=14 And NS=28) with constant radiation and varying temperature
Table 2: PV Array specifications using sharp NU-183E1

| Parameter                  | Symbol | Value      |
|----------------------------|--------|------------|
| Total peak power           | $P_{tm}$ | 71 kW      |
| Number of series strings   | $NS$   | 28         |
| Number of parallel         | $NP$   | 14         |
| Number of PV panels        | $N$    | 392        |
| Voltage in maximum power   | $V_m$  | 664 V      |
| Current peak               | $I_m$  | 107 A      |

Table 3. Maximum power points (MPP): in Figure 3 and Figure 4

| MPP | $V_m$ [V] | $P_m$ [KW] |
|-----|-----------|------------|
| M1  | 664.2     | 71         |
| M2  | 661       | 57.2       |
| M3  | 648.8     | 35.1       |
| M4  | 664.2     | 71.5       |
| M5  | 584       | 61.7       |

2.3. Modeling of three-phase grid-connected PV system

The state-space model of a three-phase grid-connected photovoltaic system shown in Figure 1 can be obtained by the dynamic equations described in (5a)-(5d):

\[
\frac{di_a}{dt} = -\frac{r}{L}i_a + \frac{v_{pv}}{3L}(2u_a - u_b - u_c) - \frac{1}{L}v_{ga} 
\]

(5a)

\[
\frac{di_b}{dt} = -\frac{r}{L}i_b + \frac{v_{pv}}{3L}(-u_a + 2u_b - u_c) + \frac{1}{L}v_{gb} 
\]

(5b)

\[
\frac{di_c}{dt} = -\frac{r}{L}i_c + \frac{v_{pv}}{3L}(-u_a - u_b + 2u_c) + \frac{1}{L}v_{gc} 
\]

(5c)

\[
\frac{dv_{pv}}{dt} = \frac{1}{C}i_{pv} - \frac{1}{C}(u_a i_a + u_b i_b + u_c i_c) 
\]

(5d)

Where: $u = \begin{cases} 1 & \rightarrow K_{st} : on; \ K_{st} : off \\ 0 & \rightarrow K_{st} : off ; \ K_{st} : on \end{cases}$

Applying the Concordia transformation to (5a-d), the instantaneous model in stationary coordinates is given by (6a)-(6b):

\[
\frac{di_a^s}{dt} = -\frac{r}{L}i_a^s + \frac{v_{pv}^s}{L}u_a - \frac{1}{L}v_{ga}^s 
\]

(6a)

\[
\frac{di_b^s}{dt} = -\frac{r}{L}i_b^s + \frac{v_{pv}^s}{L}u_b - \frac{1}{L}v_{gb}^s 
\]

(6b)

\[
\frac{di_c^s}{dt} = -\frac{r}{L}i_c^s + \frac{v_{pv}^s}{L}u_c + \frac{1}{L}v_{gc}^s 
\]

(6c)

where

\[
\begin{bmatrix} i_{a,b,c} \end{bmatrix} = \Theta_{abc}^{\alpha\beta} \begin{bmatrix} i_{a,b,c} \end{bmatrix}; \quad \begin{bmatrix} v_{a,b,c} \end{bmatrix} = \Theta_{abc}^{\alpha\beta} \begin{bmatrix} v_{a,b,c} \end{bmatrix}; \quad \begin{bmatrix} u_{a,b,c} \end{bmatrix} = \Theta_{abc}^{\alpha\beta} \begin{bmatrix} u_{a,b,c} \end{bmatrix} 
\]

(7a)

And the transformation matrix $\Theta_{abc}^{\alpha\beta}$ is given by:

\[
\Theta_{abc}^{\alpha\beta} = \frac{1}{\sqrt{3}} \begin{bmatrix} 1 & \frac{1}{2} & \frac{1}{2} \\ 0 & \frac{\sqrt{3}}{2} & -\frac{1}{2} \\ \frac{1}{\sqrt{2}} & \frac{1}{\sqrt{2}} & \frac{1}{\sqrt{2}} \end{bmatrix} 
\]

(7b)
According to the three-phase instantaneous active and reactive power theory, the instantaneous active power \( P \) and the instantaneous reactive power \( Q \) can be derived in three-phase \( abc \) coordinates for the three-phase photovoltaic grid-connected inverter:

\[
P = v_{gA}i_A + v_{gB}i_B + v_{gC}i_C
\]  
\[
Q = [(v_{gB} - v_{gA})i_A + (v_{gC} - v_{gB})i_B + (v_{gA} - v_{gC})i_C] \sqrt{3}
\]  

In the \( \alpha\beta \) coordinates, the instantaneous active power \( P \) and the instantaneous reactive power \( Q \) can be expressed as following:

\[
P = v_{gA}i_\alpha + v_{gB}i_\beta
\]  
\[
Q = v_{gA}i_\beta - v_{gB}i_\alpha
\]

3. OUTPUT FEEDBACK CONTROLLER DESIGN

The model (6a-c) is useful to build an accurate simulator for the studied system however it is not adequate to elaborate a continuous controller as it involves a binary input \( u_\alpha \) and \( u_\beta \). For control design purpose, it is more convenient to consider the following averaged model, obtained by averaging the model (6a-c) over one switching period [17].

\[
\dot{x}_1 = -r \frac{x_1}{L} + \frac{x_2}{L} u_\alpha - \frac{1}{L} v_{ga}
\]  
\[
\dot{x}_2 = -r \frac{x_2}{L} + \frac{x_3}{L} u_\beta - \frac{1}{L} v_{gb}
\]  
\[
\dot{x}_3 = -\frac{1}{C} (\mu_\alpha x_1 + \mu_\beta x_2) + \frac{1}{C} i_{pv}
\]

where \( x_1 \), \( x_2 \), \( x_3 \), \( \mu_\alpha \) and \( \mu_\beta \) denote the average values of, respectively \( i_\alpha \), \( i_\beta \), \( v_{pv} \), \( u_\alpha \) and \( u_\beta \). The signals \( \mu_\alpha \) and \( \mu_\beta \), called duty ratios which belong to \([0,1]\), are considered as the inputs of the system (10a-c).

On the basis of (10a-c), the next two subsections will be devoted to the observer design and the nonlinear controller design.

3.1. Observer design

Let us now consider in (10a-c) that is the only measurable variable. Then the following nonlinear observer is proposed:

\[
\dot{\hat{x}}_1 = -r \frac{\hat{x}_1}{L} + \frac{\hat{x}_2}{L} u_\beta - \frac{1}{L} v_{ga}
\]  
\[
\dot{\hat{x}}_2 = -r \frac{\hat{x}_2}{L} + \frac{\hat{x}_3}{L} u_\alpha - \frac{1}{L} v_{gb}
\]  
\[
\dot{\hat{x}}_3 = -\frac{1}{C} (\mu_\alpha \hat{x}_1 + \mu_\beta \hat{x}_2) + \frac{1}{C} i_{pv} + \lambda (x_3 - \hat{x}_3)
\]

Where \( \hat{x}_1 \), \( \hat{x}_2 \), \( \hat{x}_3 \) represent the estimates of the state variables and \( \lambda > 0 \) being the observer design parameter.

Let us introduce the estimation errors \( z_1 = x_1 - \hat{x}_1 \), \( z_2 = x_2 - \hat{x}_2 \) and \( z_3 = x_3 - \hat{x}_3 \). Then, from (10a-c) and (11a-c), one has:

\[Output feedback nonlinear control of three-phase grid-connected PV generator (A.Yahya)\]
\[ \dot{z}_1 = -\frac{r}{L}z_1 + \frac{z_1}{L} \mu_\alpha \]  \quad (12a)  
\[ \dot{z}_2 = -\frac{r}{L}z_2 + \frac{z_2}{L} \mu_\beta \]  \quad (12b)  
\[ \dot{z}_3 = -\frac{1}{C} \left( \mu_\alpha z_1 + \mu_\beta z_2 \right) - \lambda z_3 \]  \quad (12c)  

From the error system (12a-c), one can state the following:

**Proposition:** Consider the estimation error system (12a-c), obtained by combining the system (10a-c) and the nonlinear observer (11a-c). Then, \( \exists \lambda_0, \forall \lambda > \lambda_0 \), whatever the initial conditions, the state estimation error \( z = [z_1, z_2, z_3]^T \) converges exponentially to zero.

**Proof:** Consider the following quadratic Lyapunov function:

\[ V_o = \frac{1}{2} \sum_{i=1}^{3} z_i^2 \]  \quad (13)  

Its derivative, using (12a-c), can be obtained as follows:

\[ \dot{V}_o = -\frac{r}{L}z_1^2 - \frac{r}{L} z_2^2 - \lambda z_3^2 + \beta_1 z_1 z_3 + \beta_2 z_2 z_3 \]  \quad (14a)  

With

\[ \beta_1 = \mu_\alpha \left( \frac{1}{L} - \frac{1}{C} \right), \quad \beta_2 = \mu_\beta \left( \frac{1}{L} - \frac{1}{C} \right) \]  \quad (14b)  

Using Young’s Inequality (14a) becomes

\[ \dot{V}_o \leq -\frac{r}{L}z_1^2 - \frac{r}{L} z_2^2 - \lambda z_3^2 + \left| \beta_1 \left( \frac{1}{2 \varepsilon_1} \varepsilon_1 z_1^2 + \frac{\varepsilon_1}{2} \varepsilon_3^2 \right) \right| + \left| \beta_2 \left( \frac{1}{2 \varepsilon_2} \varepsilon_2 z_2^2 + \frac{\varepsilon_2}{2} \varepsilon_3^2 \right) \right| \]  \quad (15)  

where \( \varepsilon_1 \) and \( \varepsilon_2 \) being any real positive constants.

As \( \mu_\alpha \in [0,1] \) and \( \mu_\beta \in [0,1] \) (duty ratio functions), it follows that \( |\beta_1| \leq \beta_0 \) and \( |\beta_2| \leq \beta_0 \) where

\[ \beta_0 = \frac{1}{L} - \frac{1}{C} \]  \quad (16)  

From (15) becomes, using (16)

\[ \dot{V}_o \leq -k_1 z_1^2 - k_2 z_2^2 - k_3 z_3^2 \]  \quad (17a)  

Where

\[ k_1 = \frac{r}{L} - \frac{\beta_0}{2 \varepsilon_1}, \quad k_2 = \frac{r}{L} - \frac{\beta_0}{2 \varepsilon_2}, \quad k_3 = \lambda - \frac{\beta_0}{2} (\varepsilon_1 + \varepsilon_2) \]  \quad (17b)  

Let \( \varepsilon_1 \) and \( \varepsilon_2 \) to be chosen as follows: \( \varepsilon_1 > \frac{\beta_0 L}{2r} \) and \( \varepsilon_2 > \frac{\beta_0 L}{2r} \). Then, the observer design parameter \( \lambda \) can be chosen so that \( \lambda > \lambda_0 \) where:
\[
\lambda_0 = \frac{\beta_0}{2} (\ddot{\alpha} + \ddot{\beta})
\]

Therefore \( k_1 > 0, \ k_2 > 0 \) and \( k_3 > 0 \). It follows that (17a) can be rewritten as follows:

\[
\dot{V}_o \leq -kV_o
\]

where

\[
k = 2 \min(k_1, k_2, k_3)
\]

From (19), it is easy to show that:

\[
V'_o(t) \leq -e^{-k(t-t_0)}V'_o(t_0)
\]

which yields that \( V'_o(t) \) is exponentially vanishing. It follows that \( \lim_{t \to \infty} z(t) = 0 \), which in turn shows that the estimates converge toward their true values. This ends the proof of the Proposition. In the next subsection, we focus on elaborating a controller that stabilizes the system.

3.2. Nonlinear controller design

With the aim of design an appropriate control for the model (10a-c) described in previous section, the control objectives, the control design and stability analysis will be investigated in this Section, taking into account the nonlinear feature and the multi-input multi-output (MIMO) aspect of the system. In order to define the control strategy, the first step is to establish control objectives, which can be summarized as follows:

a. Maximum power point tracking (MPPT) of PV arrays,

b. Unity power factor (PF) in the grid,

c. Asymptotic stability of the whole system.

It is worth noting that all objectives must be achieved without sensing all variables. The PV voltage \( x_3 \) is the only measurable variable.

The first control objective is to enforce the real power \( P \) to track the maximum power point \( P_{MPP} \). It’s already point out; that this power can be controlled by the \( \alpha \)-axis current \( i_\alpha \) and \( \beta \)-axis current \( i_\beta \) (see (9a)). In this paper the MPPT algorithm based on the Perturb and Observe (P&O) technique \[18\] is resorted to generate the coefficient \( \theta \) (involved in (22)) so that the active power \( P \) tracks its maximum value i.e. \( P = P_{MPP} \).

The second control objective means that the grid currents, \( i_a, i_b \) and \( i_c \) should be sinusoidal and in phase with the AC grid voltage \( v_{gα}, v_{gβ} \) and \( v_{gγ} \) respectively. To this end the reactive power have to be null. To achieve this objectives it suffices to enforce the \( \alpha \)-axis current \( i_\alpha \) and \( \beta \)-axis current \( i_\beta \) to track reference signals, say \( x^*_1 \) and \( x^*_2 \), of the following forms:

\[
x^*_1 = \theta \cdot v_{gα}
\]

\[
x^*_2 = \theta \cdot v_{gβ}
\]

With \( \theta \) is any real positive parameter (although transient time-variations are allowed). Its generation will be seen later using the MPPT algorithm (see section 4). Once the control objectives are clearly defined, as the MIMO system is highly nonlinear, a Lyapunov based nonlinear control is proposed \[17\]. Given the observer guarantees that the errors \( z_1 = x_1 - \dot{x}_1 \) and \( z_2 = x_2 - \dot{x}_2 \) converge to zero, the following controller design will be based on the estimate variables instead of their true values. Therefore, the following errors are introduced:

\[
z_4 = \dot{x}_1 - x^*_1
\]
\[ z_5 = \dot{\hat{x}}_2 - x_2^* \]  

(25)

In order to achieve the objectives: MPPT and power factor unit, one can seek that the errors \( z_4 \) and \( z_5 \) are vanishing. To these ends the dynamics of \( z_4 \) and \( z_5 \) have to be clearly defined. Deriving (24) and (25), it follows from (11a) and (11b) that:

\[ \dot{z}_4 = -\frac{r}{L} \dot{x}_1 + \frac{\dot{x}_1}{L} \mu_a - \frac{1}{L} v_{in} - \dot{\hat{x}}_1^* \]  

(26)

\[ \dot{z}_5 = -\frac{r}{L} \dot{x}_2 + \frac{\dot{x}_1}{L} \mu_\beta - \frac{1}{L} v_{bg} - \dot{\hat{x}}_2^* \]  

(27)

The goal, now, is to make \( z_4 \) and \( z_5 \) exponentially vanishing by enforcing its derivatives \( \dot{z}_4 \) and \( \dot{z}_5 \) to behave as follows:

\[ \dot{z}_4 = -\rho_1 \text{sgn}(z_4) - \xi_1 \int z_4(\tau) d\tau \]  

(28)

\[ \dot{z}_5 = -\rho_2 \text{sgn}(z_5) - \xi_2 \int z_5(\tau) d\tau \]  

(29)

where \( \rho_1 > 0 \), \( \rho_2 > 0 \), \( \xi_1 > 0 \) and \( \xi_2 > 0 \) being design parameters and is a signum function. It is worth noting that the integral actions are introduced in (28) and (29) to allow a good robustness of the controller against unmodeled dynamics and perturbations. Combining (26) and (28) the first control law \( \mu_a \) is obtained:

\[ \mu_a = \frac{L}{\dot{x}_1}\left(-\rho_1 \text{sgn}(z_4) + \frac{r}{L} \dot{x}_1 + \frac{1}{L} v_{in} + \ddot{x}_1^* - \xi_1 \int z_4(\tau) d\tau \right) \]  

(30)

Finally, combining (27) and (29), the second control law \( \mu_\beta \) is also obtained

\[ \mu_\beta = \frac{L}{\dot{x}_1}\left(-\rho_2 \text{sgn}(z_5) + \frac{r}{L} \dot{x}_2 + \frac{1}{L} v_{bg} + \ddot{x}_2^* - \xi_2 \int z_5(\tau) d\tau \right) \]  

(31)

Since the control laws are clearly defined, the concern now is to investigate the convergence of the errors \( z_4 \) and \( z_5 \). To this end the following quadratic Lyapunov function is considered

\[ V_C = \frac{1}{2} z_4^2 + \frac{1}{2} z_5^2 + \frac{\xi_1}{2} \left[ z_4(\tau) d\tau \right]^2 + \frac{\xi_2}{2} \left[ z_5(\tau) d\tau \right]^2 \]  

(32)

Its derivative is obtained as follows Its derivative is obtained as follows:

\[ \dot{V}_C = z_4 \dot{z}_4 + z_5 \dot{z}_5 + \xi_1 z_4 \left[ z_4(\tau) d\tau \right] + \xi_2 z_5 \left[ z_5(\tau) d\tau \right] \]  

(33)

which, using (28) and (29), gives:

\[ \dot{V}_C = -\rho_1 |z_4| - \rho_2 |z_5| \]  

(34)

As \( V_C \) is positive definite function and its derivative (34) is negative definite it follows that the equilibrium \( \langle z_4, z_5 \rangle = (0, 0) \) is globally asymptotically stable [18]. Which, in turn, gives \( \lim_{t \to \infty} (z_4(\tau), z_5(\tau)) \to (0, 0) \)

The main result of the proposed output feedback controller is summarized in the following theorem.
Theorem: Consider the closed-loop system consisting of the controlled system of Figure 1 represented by its nonlinear model (10a-c), the nonlinear observer (11a-c) and the controller composed of the control laws (30) and (31). Then, one has:

a. The closed loop system is GAS. It follows that all closed loop signals are bounded.

b. The estimation errors \( z = [z_1, z_2, z_3]^T \) converges exponentially to zero.

c. The tracking errors \( z_4 \) and \( z_5 \) converge to zero implying MPPT achievement and power factor unit.

Proof: let us consider the following quadratic Lyapunov function:

\[
V = V_O + V_C = \frac{1}{2} \sum_{i=1}^{5} z_i^2 + \frac{\xi}{2} \int z_4(t)dt^2 + \frac{\xi}{2} \int z_5(t)dt^2
\]  

(35)

Its derivative, using (19) and (34), can be obtained as follows:

\[
\dot{V} = \dot{V}_O + \dot{V}_C \leq -k \left( z_1^2 + z_2^2 + z_3^2 \right) - \rho_1 |z_4| - \rho_2 |z_5|
\]  

(36)

Which clearly shows that, the equilibrium \( z = 0 \) of the closed loop system with the state error vector \( z = [z_1, z_2, z_3, z_4, z_5]^T \) is globally asymptotically stable. It follows that all errors are vanishing. This ends the proof of theorem. The next section devoted to the performances evaluation of the proposed output feedback controller.

4. SIMULATION RESULTS

The theoretical performances described by the theorem of an output feedback controller, including the control laws (30-31) and the nonlinear observer (11a-c), designed in Section 3, are now illustrated by simulation. The experimental setup, described by Figure 5, is simulated using MATLAB/SIMULINK. The characteristics of the controlled system are listed in Table 4. Note that the controlled system is simulated using.

![Simulation bench of the proposed three-phase grid connected system](image)

Figure 5. Simulation bench of the proposed three-phase grid connected system

The instantaneous three phase model given by (5a-d). The model (10a-c) in \( \alpha-\beta \) axis is only used in the controller design. The design parameters of the controller are given values of Table 5. These parameters have been selected using a ‘trial-and-error’ search method and proved to be suitable. It worth noting that the parameter \( \theta \) involved in (22) and (23) is generated using Perturb and Observe algorithm with the block-diagram illustrated by Figure 6. The resulting closed loop control performances are illustrated by Figure 7 to Figure 13.
Table 4. Characteristics of controlled system

| Parameter          | Symbol  | Value  |
|--------------------|---------|--------|
| PV array           | PV power| 40 kW  |
| DC link capacitor  | C       | 3300μF |
| Grid filter inductor | L         | 3mH   |
| PWM                | r       | 0.2Ω   |
| Grid               | AC source | 220V |
| Line frequency     |         | 50Hz   |

Figure 6. P&O algorithm implementation in Matlab/Simulink software

Table 5. Controller parameters

| Parameter          | Symbol  | Value  |
|--------------------|---------|--------|
| Design parameters  |         |        |
| $\rho_1$           |         | $10^3$ |
| $\rho_2$           |         | $4 \times 10^4$ |
| $\xi_1$            |         | 0.1    |
| $\xi_2$            |         | 0.1    |
| $\lambda$          |         | $5 \times 10^5$ |
| P&O algorithm parameters | Delay time $T_o$ | $10^{-4}$ |
|                     | Step value $k$ | 0.3    |

4.1. Radiation change effect

Figure 7 shows the perfect MPPT in the presence of radiation step changes meanwhile, the temperature is kept constant, equal to 298.15K(25°C). The simulated radiation profile is as follow: a first step change is performed between 500 and 1000W/m² at time $t = 0.1$ s and the second one between 1000 and 800 W/m² at time $t = 0.2$ s. The Figure 8 shows that the PV power captured varies between 35.1 kW and 71 kW and then returns to 57.2 kW. These values correspond is shows in Figure 3 to maximum points (M3, M1 and M2) of the curves associated to the considered radiation, respectively. The Figure 8 also shows that the voltage of the PV array $V_{pv}$ varies between $V_{pv} = 648.8$ V and $V_{pv} = 664$ V and then returns to 661V, which correspond very well to the optimum voltages. Figure 9. shows the injected current $i_a$ and the grid voltage $v_{ga}$. This Figure 9 clearly shows that the grid current $i_a$ is sinusoidal and in phase with the grid voltage $v_{ga}$, proving that the power factor unit is achieved. The alternating currents injected to the grid are illustrated by Figure 10.
Figure 7. State variables and their estimates in transitional regime and in presence of radiation step changes

Figure 8. MPPT capability of the controller in presence of radiation step changes

Figure 9. Unity PF achievement in presence of radiation step changes

Output feedback nonlinear control of three-phase grid-connected PV generator (A. Yahya)
4.2. Temperature variation effect

Figure 11 shows the performances of the controller in presence of temperature step changes while the radiation λ is kept constant equal to 1000W/m². The temperature step change is performed at time t=0.15s between T=25°C (298.15K) and T=55°C (328.15K). It is worth noting that these changes are very abrupt which is not realistic in practical case. Nevertheless, with this important change we want to show a good robustness of the proposed controller to achieving the MPPT objective. It can be seen from Figure 11 that the system tracks the new operating point very quickly. Indeed, the captured PV power P achieves the values 71.7kW et 61.7kW corresponding to the maximum points (M4 and M5) associated to the temperatures 25°C and 55°C, respectively as shown in Figure 4.
Figure 12 illustrates the grid current $i_a$ and the grid voltage $v_{ga}$. Figure 12 also shows that the current $i_a$ is sinusoidal and in phase with the voltage $v_{ga}$ which proves the unity PF requirement. Finally, Figure 13 shows the zoomed three phase’s grid currents and voltages.

5. CONCLUSION

We have addressed the problem of current sensorless control of the photovoltaic energy conversion system. The main feature of the system presented is it does not require an intermediate stage of DC-DC control, because the maximum power is set by the inverter itself by means of a Perturb & Observe algorithm.

The system dynamics has been described by the nonlinear state-space model (5a-b). Based on a transformed model in $\alpha-\beta$ axis, an output feedback controller, combining an observer and a state feedback control laws is designed and analyzed using a Lyapunov approach. The controller objectives are threefold: i) ensuring the MPPT in the side of PV generator; ii) guaranteeing a power factor unit in the side of the grid, iii) ensuring the global asymptotic stability of the closed loop system. Using both formal analysis and simulation, it has been proven that the obtained controller meets all the objectives. It is worth noting that all objectives are achieved without resorting to the measurement of all variables. The use of the estimator is motivated by the global cost and reliability considerations. Indeed, the fewer the number of sensors, the lower the global cost.

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