Abstract—This article is concerned with a new optimization problem named “phase change rate maximization” for single-input–single-output linear time-invariant systems. The problem relates to two control problems, namely robust instability analysis against stable perturbations and minimum-norm strong stabilization. We define an index of the instability margin called “robust instability radius (RIR)” as the smallest $\ell_\infty$-norm of a stable perturbation that stabilizes a given unstable system. This article has two main contributions. It is first shown that the problem of finding the exact RIR via the small-gain condition can be transformed into the problem of maximizing the phase change rate at the peak frequency with a phase constraint. Then, we show that the maximum is attained by a constant or a first-order all-pass function and derive conditions, under which the RIR can be exactly characterized, in terms of the phase change rate. Two practical applications are provided to illustrate the utility of our results.

Index Terms—Instability analysis, Nyquist criterion, phase change rate (PCR) maximization, robust control, strong stabilization.

I. INTRODUCTION

Feedback is essential and inevitable for maintaining the desired behaviors against uncertainties in the target systems and/or disturbances from the environment as well as for stabilizing an unstable system. Most traditional control theories focus on regulation around an equilibrium point or tracking a class of reference signals. Robust control theory in particular provides systematic methods for analyzing and synthesizing feedback systems with guaranteed stability and control performance in the presence of model uncertainties (see, e.g., [1]). The most fundamental problem is the robust stability analysis: How much uncertainty can be allowed while maintaining stability? The answer, called the robust stability radius, has been exactly characterized by the small gain theorem, and the robust stability problem has been well understood.

A fundamental counterpart, the robust instability analysis, is to investigate the maximum allowable perturbation for a given unstable feedback system to maintain its instability. The problem has been much less studied so far, but is of engineering significance. Over the last two decades, feedback control to maintain nonequilibrium state, such as periodic oscillation has garnered more recognition as an important design problem for engineering applications including robotic locomotion [2], [3] and as an interesting issue in synthetic biology (see, e.g., [4], [5], and [6]). Robustness of such nonequilibrium states is difficult to analyze in general. However, robust instability analysis for linear systems works fairly well for maintaining certain classes of nonlinear oscillations as demonstrated in [7] and [8], where robust oscillations in the sense of Yakubovich are guaranteed by instability of equilibria and ultimate boundedness [9]. Moreover, as a byproduct of the robust instability analysis, the search for the worst case stable perturbation provides a solution to the strong stabilization, a long-standing problem of practical relevance.

Given the above background, the main focus of this article is the analysis of the instability margin, which poses challenges as described below.

(i) Robust Instability Analysis: The problem is similar to but quite different from that of robust stability analysis as pointed out in [7], which demonstrated through numerical examples why robust instability analysis is far more difficult. Unlike robust stability analysis, the small gain condition in terms of the $L_\infty$-norm only gives a lower bound of the robust instability radius (RIR) (as seen in e.g., [10] and [11]), because existence of a purely imaginary pole does not necessarily imply transition from instability to stability (although the opposite transition is implied). Therefore, characterization of the RIR requires an intricate analysis to ensure not one but all of unstable poles are perturbed to the left half plane.
(ii) Stabilization by a Minimum-Norm Stable Controller: The difficulty of the RIR analysis can be understood by its equivalence to the minimum-norm strong stabilization problem, [7], [8] where a stable controller with minimum norm is sought to stabilize a given unstable plant. Although the necessary and sufficient condition for strong stabilizability is known to be the parity interlacing property (PIP) for single-input-single-output (SISO) systems, the required order of a strongly stabilizing controller is unknown [12], [13]. It is also unknown whether the problem of strong stabilization can be transformed into a convex optimization problem. Hence, no computationally efficient algorithm is known for solving such a problem. Minimization of the $H_{\infty}$-norm on some closed-loop transfer functions has been considered in the literature, but only partial solutions have been obtained for the problem in hand due to the difficulty in enforcing the stability constraint on the controller, e.g., [14]. Hence, the requirement of strong stabilization with norm constraint on the controller makes the optimization problem extremely difficult. The instability margin analysis can be formalized by defining the RIR in a manner analogous to the classical robust stability radius for $H_{\infty}$-norm bounded perturbations [15]. A sufficient condition that allows for exact calculation of the RIR is given in [8]. The main idea was to find a first-order all-pass function, which marginally stabilizes a given unstable system, and the article presented a class of third-order systems to meet the condition with an application to the repressilator [5], showing the effectiveness of this approach.

In this article, we provide conditions on SISO systems of which the RIR may or may not be given by the small gain condition, under a very mild assumption that the class of systems is restricted to those for which the peak gain occurs at a single frequency. In the cases where it may, a worst-case perturbation turns out to be a constant or a first-order all-pass function, justifying the aforementioned idea outlined in [8].

There are two main theoretical contributions in this article. The first contribution is to show that the problem of finding the exact RIR may be turned into the problem of maximizing the phase change rate (PCR) at the peak frequency subject to a phase constraint. The fundamental tool to show this is an extended version of the Nyquist criterion for the marginal stability. It should be emphasized that the problem of PCR maximization is a completely new problem, which has not been investigated in the past. The second contribution is to provide a complete solution of the maximization problem. We will prove that the supremum is attained by a constant or a first-order all-pass function, and derive conditions in terms of the PCR, under which the exact RIR is attained. It is somewhat surprising that no higher order all-pass function could achieve better PCR than a constant or a first-order function. This is due to the phase constraint imposed at the peak gain frequency. This point will be clarified when we solve the maximization problem.

To illustrate the applicability of our results, two practical applications are considered. The first one regards the robustness of the oscillatory behavior of a cyclic gene-regulatory network called “repressilator.” We apply our results to analyze robustness of the instability of the linearized dynamics against dynamic perturbations. The second one regards strong stabilization of a magnetic levitation system, where we demonstrate how our results can be useful for the design of stable discrete-time controllers with small $H_{\infty}$ norms.

The rest of this article is organized as follows. Section II defines the RIR and briefly summarizes results in [8] as a basis for the developments in this article. Section III characterizes the open-loop transfer functions that yield marginally stable closed-loop systems, based on an extended version of the Nyquist criterion. The main results of this article on the conditions for marginal stabilization and the exact RIR are presented in Section IV. In Section V, we formulate a problem of maximizing the PCR and provide a solution, which plays an essential role in the proofs of the main results in Section IV. Two practical applications of our main results are given in Section VI. Proofs of our main results are given in Section VII. Finally, Section VIII concludes this article and addresses some future research directions.

Notation: The set of real numbers is denoted by $\mathbb{R}$, $\mathbb{R}(s)$ and $\Im(s)$ denote the real and imaginary parts of a complex number $s$, respectively. The set of proper real rational functions of complex variable $s$ is denoted by $\mathcal{R}_{p}$. Let $\mathcal{L}_{\infty}$ denote the set of functions that are bounded on the imaginary axis $j\mathbb{R}$. The subset of $\mathcal{L}_{\infty}$, which consists of real rational functions that are bounded on $j\mathbb{R}$, is denoted by $\mathcal{R}\mathcal{L}_{\infty}$. The stable subsets of $\mathcal{L}_{\infty}$ and $\mathcal{R}\mathcal{L}_{\infty}$ are denoted by $\mathcal{H}_{\infty}$ and $\mathcal{R}\mathcal{H}_{\infty}$, respectively. The norms in $\mathcal{L}_{\infty}$ and $\mathcal{H}_{\infty}$ are denoted by $\|\cdot\|_{\mathcal{L}_{\infty}}$ and $\|\cdot\|_{\mathcal{H}_{\infty}}$, respectively. The open (closed) left and right half complex planes are abbreviated as OLH (CLH) and ORH (CRH), respectively.

II. RIR: DEFINITION AND PRELIMINARY RESULTS

We consider a positive feedback system with perturbed loop transfer function $\tilde{h}(s)$, represented by the upper linear fractional transformation (LFT)

$$\tilde{h}(s) = \mathcal{F}_u\left(\begin{bmatrix} h_{11}(s) & h_{12}(s) \\ h_{21}(s) & h(s) \end{bmatrix}, \delta(s) \right)$$

$$= h(s) + h_{21}(s)\delta(s)(1 - h_{11}(s)\delta(s))^{-1}h_{12}(s)$$

(1)

where $h(s)$ is the scalar nominal loop transfer function and $\delta(s)$ denotes the norm-bounded stable perturbation. The LFT representation (1) covers a variety of perturbations, including

Multiplicative-type: $$\tilde{h}(s) = (1 + w_m(s)\delta(s))h(s)$$

Feedback-type: $$\tilde{h}(s) = h(s)/(1 + w_f(s)\delta(s))$$

where $h_{11}(s)$, $h_{12}(s)$, and $h_{21}(s)$ are, respectively, set as $(h_{11}, h_{12}, h_{21}) = (0, h, w_m)$ and $(-w_f, -w_f, h)$.

We here assume that the nominal feedback system is strictly unstable, i.e., the corresponding characteristic equation $1 - h(s) = 0$ has at least one root in the ORHP, and we consider the problem of determining the minimum norm of $\delta(s)$, which makes the feedback system stable. Note that the characteristic equation of the perturbed system $1 - \tilde{h}(s) = 0$ can be re-expressed as

$$\delta(s)g(s) = 1$$

(2)
where \( g(s) \) is an unstable transfer function given by
\[
g(s) := h_{11}(s) + h_{21}(s)h_{12}(s)/(1 - h(s)).
\]
Clearly, the weighted sensitivity and complementary sensitivity functions, \( g_f(s) := w_f(s)/(1 - h(s)) \) and \( g_m(s) := w_m(s)h(s)/(1 - h(s)) \), play an important role in the robust instability analysis in the same way as in the robust stability analysis. We also note that (2) presents the strong stabilization problem, where \( g(s) \) and \( \delta(s) \) correspond to an unstable plant and a stable stabilizing controller to be designed, respectively. In what follows, our theoretical investigation is based on (2).

The rest of the section briefly summarizes some concepts and results from [7] and [8], which form a basis for the developments in this article. Consider a class of unstable systems defined by
\[
G := \{ g \in \mathcal{RL}_\infty \mid g \text{ is strictly proper and unstable} \}. \tag{3}
\]
The RIR for \( g \in G \), denoted by \( \rho_s(g) \in \mathbb{R} \), with respect to real rational dynamic perturbation \( \delta \in \mathcal{RH}_\infty \), is defined as the smallest magnitude of the perturbation that internally stabilizes the system
\[
\rho_s(g) := \inf_{\delta \in \mathcal{S}(g)} ||\delta||_{\mathcal{H}_\infty}
\]  \tag{4}
where \( \mathcal{S}(g) \) is the set of real-rational, proper, stable transfer functions internally stabilizing \( g \), i.e.,
\[
\mathcal{S}(g) := \{ \delta \in \mathcal{RH}_\infty : \delta(s)g(s) = 1 \Rightarrow \Re(s) < 0, \delta(s) = 0, \Re(s) > 0 \Rightarrow |g(s)| < \infty \}.
\]  \tag{5}
It is noticed from the well known result on strong stabilizability in [12] that \( \rho_s(g) \) is finite if and only if the PIP is satisfied, i.e., the number of unstable real poles of \( g \) between any pair of real zeros in the CRHP (including zero at \( \infty \)) is even. Consequently, the class of systems of our interest is defined as
\[
G_n := \{ g \in G \mid g \text{ has } n \text{ unstable poles and satisfies the PIP condition} \}. \tag{6}
\]
where \( n \) is a natural number. We aim to give conditions on \( g \in G_n \), under which the RIR can be characterized exactly by the lower bounds given analytically as follows:

Lemma 1 (see [8]): Let \( g \in G \) be given. Then
\[
\rho_s(g) \geq g_p := 1/||g||_{L_\infty}, \quad ||g||_{L_\infty} := \sup_{\omega \in \mathbb{R}} |g(j\omega)|.
\]  \tag{7}
Moreover, if \( g \in G \) has an odd number of unstable poles (counting multiplicity), then we have
\[
\rho_s(g) \geq g_o := 1/|g(0)|.
\]  \tag{8}
Let us introduce some notions of stability to facilitate clear and rigorous presentation of our theoretical developments.

Definition 1:
- A rational function \( h \in \mathbb{R}_p \) is called “exponentially stable” if all the poles of \( h \) are in the OLHP.
- A rational function \( h \in \mathbb{R}_p \) is called “exponentially unstable” if at least one of the poles of \( h \) is in the ORHP.
- A rational function \( h \in \mathbb{R}_p \), which is neither exponentially stable nor exponentially unstable is called “marginally stable” if any pole of \( h \) on the imaginary axis is simple.
- A marginally stable rational function \( h \) is called “single mode marginally stable,” if all the poles are located in the OLHP except for either a pole at the origin or a pair of complex conjugate poles on the imaginary axis, say \( \pm j\omega_c \).

To specify the mode on the imaginary axis, the system is called \( \omega_c \)-marginally stable with \( \omega_c = 0 \) for the former and \( \omega_c \neq 0 \) for the latter.
- A rational function \( h \in \mathbb{R}_p \), which is neither exponentially stable nor exponentially unstable is called “polynomially unstable” if at least one of the poles of \( h \) on the imaginary axis is not simple.

An upper bound on the RIR is obtained as \( ||\delta||_{\mathcal{H}_\infty} \), if a stable stabilizing perturbation \( \delta \in \mathcal{S}(g) \) is found. The following proposition presented in [8] shows that an upper bound can always be obtained if marginal stability is achieved with a single mode on the imaginary axis.

Proposition 1 (see [8]): Consider real-rational transfer functions \( g \) and \( \delta \), having no unstable pole/zero cancelation between them, where the former is strictly proper and the latter is proper and stable (possibly a real constant). Suppose, the positive feedback system with loop transfer function \( \delta, g \) is single mode marginally stable. Then, for almost\(^1\) proper any proper stable transfer function \( \delta_1 \), there exists \( \varepsilon \in \mathbb{R} \) of arbitrarily small magnitude \( |\varepsilon| \), such that the positive feedback with \( \delta_\varepsilon := \delta_0 + \varepsilon \delta_1 \) internally stabilizes \( g \).

Note that marginal stability requires that the transfer function \( \delta_0 \) be chosen to satisfy
\[
\delta_0(j\omega_c) = \delta_\varepsilon := 1/g(j\omega_c)
\]  \tag{9}
at a critical frequency \( \omega_c \geq 0 \), so that \( s = j\omega_c \) is a closed-loop pole. If we parameterize a class of perturbations, then \( \delta_\varepsilon \), satisfying (9) may be determined for each \( \omega_c \in \mathbb{R} \), and an upper bound \( ||\delta_\varepsilon||_{\mathcal{H}_\infty} \) on the RIR is obtained when the resulting closed-loop poles (i.e., roots of \( \delta_\varepsilon(s)g(s) = 1 \)) are all in the OLHP, except for \( s = \pm j\omega_c \). Note that the exact RIR of \( g \) is obtained if \( ||\delta_\varepsilon||_{\mathcal{H}_\infty} \) coincides with one of the lower bounds, such as those stated in Lemma 1. In this article, we will focus on the single mode marginal stabilization to derive conditions for getting the exact RIR.

III. OPEN-LOOP CHARACTERIZATION OF MARGINALLY STABLE CLOSED-LOOP SYSTEMS

In this section, we present an extended version of the Nyquist criterion for characterizing single mode marginal stability. The result will be used in Section IV to derive synthesis conditions on the certain classes of open-loop systems, which eventually leads to conditions that characterize the exact RIR of these systems.

\(^1\)This means that an arbitrarily chosen \( \delta_1 \) may or may not work to stabilize, but when it does not work, a slight modification of it can always make it work.
A. Gain/Phase Change Rates

This section introduces the gain and PCRs for an $\mathcal{RL}_\infty$ function, which are useful for characterizing the single mode marginal stability.

For a complex function $f: \mathbb{C} \to \mathbb{C}$, the logarithmic gain and the phase angle at point $s \in \mathbb{C}$, such that $f(s) \neq 0$ are defined as $\ln |f(s)|$ and $\angle f(s)$, respectively. Here, the angle $\angle f(s)$ of the complex number $f(s)$ is not uniquely determined but is chosen, so that $\angle f(j\omega)$ is continuous on $\omega \in \mathbb{R}$; such a choice is possible for $f \in \mathcal{RL}_\infty$ with no zeros on the imaginary axis. For $f(s) \neq 0$, $\log f(s) := \ln |f(s)| + j \cdot \angle f(s)$. Let us denote the logarithmic gain and the phase of frequency response $f(j\omega)$ by

$$A_f(\omega) := \ln |f(j\omega)|, \quad \theta_f(\omega) := \angle f(j\omega). \quad (10)$$

In order to characterize how these quantities change when $s = j\omega$ is perturbed in the direction parallel to the real or imaginary axis, we consider the logarithmic gain and phase at point $s = \sigma + j\omega \in \mathbb{C}$, and introduce two real functions of two real variables as

$$\dot{A}_f(\sigma,\omega) := \ln |f(\sigma + j\omega)|, \quad \dot{\theta}_f(\sigma,\omega) := \angle f(\sigma + j\omega). \quad (11)$$

There are four possible directional derivatives $A'_f(\omega)$, $\theta'_f(\omega)$, $M'_f(\omega)$, and $\phi'_f(\omega)$ for a complex function $f \in \mathcal{RL}_\infty$, which are referred to as gain, phase, $\sigma$-gain, and $\sigma$-phase change rates (CRs), respectively, and defined as

$$A'_f(\omega) := \frac{\partial A_f}{\partial \sigma}(0,\omega), \quad \theta'_f(\omega) := \frac{\partial \theta_f}{\partial \sigma}(0,\omega),$$

$$M'_f(\omega) := \frac{\partial A_f}{\partial \omega}(0,\omega), \quad \phi'_f(\omega) := \frac{\partial \theta_f}{\partial \omega}(0,\omega). \quad (13)$$

Applying the Cauchy–Riemann equations (see e.g., [16]) to the complex function $\log f(s)$, we have the following relations among these four CRs.

Lemma 2: For $f \in \mathcal{RL}_\infty$, the following two relations hold for all $\omega$ satisfying $f(j\omega) \neq 0$:

$$M'_f(\omega) = \theta'_f(\omega), \quad \phi'_f(\omega) = -A'_f(\omega). \quad (14)$$

The features and roles of the four CRs are as follows.

- The phase CR, $\theta'_f(\omega)$, which represents the PCR along the horizontal line parallel to the real axis, is equal to $\theta_f'(\omega)$. Hence, its importance is the same as that of the standard phase CR. In general, the $\sigma$-gain CR is easier to handle and compute than the phase CR, and hence, the $\sigma$-gain CR is often utilized in the proofs of lemmas and theorems in this article.

- The $M'_f(\omega)$, which represents the gain CR along the imaginary axis, is instrumental for one of the key results. It relates to the phase CR through an integral relationship (a counterpart of the well-known Bode’s gain/phase integral relationships) as shown below.

- The $\sigma$-phase CR, $\phi'_f(\omega)$, represents the PCR along the horizontal line parallel to the real axis. It is the negative of the gain CR, and it is the least important among the four CRs in the development of main results of this article.

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It should be emphasized that the gain and PCRs, $A'_f(\omega)$ and $\theta'_f(\omega)$, are not independent for minimum-phase functions. We have the following integral relationship linking $\theta'_f(\omega)$, $A'_f(\omega)$, and $f(j\omega)$.

Lemma 3 (Gain/PCR integral relationships): Let $f \in \mathcal{RH}_\infty$ be a minimum-phase function. For an arbitrary $\omega_p \in \mathbb{R}$, we have

$$\theta'_f(\omega_p) = \frac{2}{\pi} \int_0^\infty \frac{\omega A'_f(\omega)}{\omega^2 - \omega_p^2} d\omega. \quad (15)$$

Furthermore, if $\omega_p$ is such that $|f(j\omega_p)| = 1$, i.e., $A_f(\omega_p) = 0$, we have

$$\theta'_f(\omega_p) = \frac{2}{\pi} \int_0^\infty \frac{\omega^2 + \omega_p^2}{(\omega^2 - \omega_p^2)^2} d\omega. \quad (16)$$

Proof: See Appendix A.

The relations (15) and (16) will be used in the proof of Lemma 10 as one of powerful tools to derive the main theorem of this article.

B. Marginal Stability Criteria Via PCR

We first establish necessary conditions and a necessary and sufficient condition for a given positive feedback system with unstable loop transfer function being either exponentially stable or marginally stable based on the Nyquist plot as a preliminary investigation for our analysis in this article.

Let us define $\nu_+(-\cdot)$ (and, respectively, $\nu_-(-\cdot)$) as the number of transverse crossing points on the real semi-interval $(1, +\infty)$ from the negative imaginary region to the positive one (respectively, from the positive to the negative) for the Nyquist plot of $L(j\omega + \cdot)$. Let $\nu_0 := \nu_+(\cdot) - \nu_-(\cdot)$.

Lemma 4: Consider a positive feedback system with loop transfer function $L \in \mathcal{G}_n$. The feedback system has all poles in the CLHP if and only if there exists $\epsilon_0 > 0$, such that the following two equivalent conditions hold for all $\epsilon \in (0, \epsilon_0]$.

(i) The number of counter-clockwise encirclements of the Nyquist plot of $L(j\omega + \epsilon)$ about $1 + j0$ is equal to $n$, the number of unstable poles of $L$.

(ii) $\nu_0(\epsilon) = n$ for the Nyquist plot of $L(j\omega + \epsilon)$.

Moreover, the feedback system is marginally stable if and only if the following two conditions hold in addition to condition (i) or (ii): (iia) $\exists \omega$, such that $L(j\omega) = 1$; (iib) If $L(j\omega) = 1$, $\frac{d}{d\omega}L(s)|_{s=j\omega} \neq 0$.

Proof: See Appendix B.

Conditions (i) and (ii), in terms of the “perturbed” Nyquist plot $L(j\omega + \epsilon)$ with small $\epsilon > 0$ can be viewed as an extended version of the Nyquist criteria for the closed-loop poles being in the CLHP. The conditions are obtained by applying Cauchy’s argument principle with a perturbed Nyquist contour to deal with closed-loop poles on the imaginary axis. Condition (iia) is equivalent to the existence of a closed-loop pole on the imaginary axis, whereas condition (iib) is equivalent to the imaginary-axis
pole(s) being simple. Building on Lemma 4, the following result gives a condition for \( \omega_c \)-marginal stability.

**Proposition 2:** Let \( \omega_c \geq 0 \), integer \( n \geq 1 \), and transfer function \( L \in \mathcal{G}_n \) be given. Consider a positive feedback system with loop transfer function \( L \). Suppose

\[
A'_L(\omega_c) = 0,
\]

i.e.,

\[
\left. \frac{d}{d\omega} |L(j\omega)| \right|_{\omega = \omega_c} = 0.
\]

Then, the feedback system is \( \omega_c \)-marginally stable if and only if condition (i) and one of conditions (ii-a) and (ii-b), indicated below, are satisfied.

(i) The loop transfer function \( L \) satisfies the following:

\[
L(j\omega_c) = 1,
\]

\[
L'(j\omega) \neq 0 \quad \forall \omega \neq \pm \omega_c.
\]

(ii-a) The Nyquist plot of \( L(j\omega) \) satisfies either \( \nu_o(0) = n - 1 \) if \( \omega_c = 0 \), or \( \nu_o(0) = n - 2 \) if \( \omega_c > 0 \), and the PCR at \( \omega = \omega_c \) is positive, i.e.,

\[
\theta'_L(\omega_c) > 0.
\]

(ii-b) The Nyquist plot of \( L(j\omega) \) satisfies \( \nu_o(0) = n \), and the PCR at \( \omega = \omega_c \) is negative, i.e.,

\[
\theta'_L(\omega_c) < 0.
\]

**Proof:** See Appendix C for a proof.

The conditions are obtained by enforcing the extended Nyquist criteria through the sensitivity analysis at the critical point \( L(j\omega_c) = 1 \), resulting in the conditions on the PCR \( \theta'_L(\omega_c) \).

The idea for the sensitivity analysis can be illustrated by several patterns shown in Fig. 1. Under (18), the Nyquist plot of \( L(j\omega) \) passes through the critical point \( 1 + j0 \) (red dot) at \( \omega = \pm \omega_c \), once \( \omega_c = 0 \) or twice \( \omega_c > 0 \). With a small \( \epsilon > 0 \), the Nyquist plot of \( L(j\omega + \epsilon) \) is a slightly perturbed version of \( L(j\omega) \) with its shape remaining similar, and hence, can still be approximately represented by the blue curve if the real axis is shifted accordingly. When \( \theta'_L(\omega_c) \) is positive/negative, the real-axis crossing point \( L(j\omega_c + \epsilon) \) is perturbed to the right/left to become \( L(j\tilde{\omega} + \epsilon) \) such that \( \tilde{\omega} = \omega_c \). This means that the location of the critical point \( 1 + j0 \) relative to the perturbed Nyquist plot \( L(j\omega + \epsilon) \) with small \( \epsilon > 0 \) can be visualized as the green dot relative to the blue curve in Fig. 1.

Now, for \( \omega_c \)-marginal stability, \( 1 + j0 \) should be encircled \( n_c \) times by the perturbed Nyquist plot \( L(j\omega + \epsilon) \) (see Lemma 4). This happens if the crossing of \( 1 + j0 \) by \( L(j\omega) \) at \( \omega = \omega_c \) is either (ii-a) upward \( (\theta'_L(\omega_c) > 0) \) with \( \nu_o(0) = n - n_c \), where \( n_c \) is the number of times \( L(j\omega) \) passing through \( 1 + j0 \), or (ii-b) downward \( (\theta'_L(\omega_c) < 0) \) with \( \nu_o(0) = n \), as shown in Fig. 1.

Single model marginal stabilization will be our main focus in the next section, which is instrumental for obtaining the exact RIR of certain classes of systems.

**IV. MAIN RESULTS**

In this section, Proposition 2 is applied to find conditions for marginal stabilizability of \( g \) belonging to some subclass of \( \mathcal{G}_n \). This in turn leads to the exact RIR of \( g \). Specifically, we will consider the subclasses of \( \mathcal{G}_n \) where each system has a unique peak frequency. To this end, we define the following two subsets of \( \mathcal{G}_n \):

\[
\mathcal{G}^0_n := \{ g \in \mathcal{G}_n \mid \|g\|_{L_\infty} = \|g(0)\| > \|g(j\omega)\| \quad \forall \omega \neq 0 \}
\]

\[
\mathcal{G}^\#_n := \{ g \in \mathcal{G}_n \mid \exists \omega_p > 0, \text{ such that} \|g\|_{L_\infty} = \|g(j\omega_p)\| > \|g(j\omega)\| \quad \forall \omega \neq \pm \omega_p \}.
\]

The assumption on the unique peak frequency is not unreasonable, as most practical systems in reality are expected to have such a characteristic. The case where a system has multiple peak frequencies is discussed in Remark 6 after the presentation of our main results.

**A. Conditions for Marginal Stabilization**

The following theorem provides necessary and sufficient conditions for marginal stabilizability of system \( g \) in \( \mathcal{G}^0_n \) or \( \mathcal{G}^\#_n \), by some system \( f \) satisfying \( \|f\|_{H_\infty} = 1/\|g\|_{L_\infty} \). As \( 1/\|g\|_{L_\infty} \) is a lower bound on the RIR of \( g \), single mode marginal stabilizability of a \( g \) by such \( f \) implies that \( g \) has the exact RIR equal to \( 1/\|g\|_{L_\infty} \) by Proposition 1.

**Theorem 1:**

(I) Given \( g \in \mathcal{G}^0_n \), \( g \) can be marginally stabilized by a stable system \( f \) with \( \|f\|_{H_\infty} = 1/\|g\|_{L_\infty} = 1/\|g(0)\| \) if and
only if \( n = 1 \) and
\[
\theta'_g(0) > 0. \tag{23}
\]

(II) Given \( g \in G_n^m \) for which the peak gain occurs at \( \omega_p \), \( g \) can be marginally stabilized by a stable system \( f \) with 
\[
\|f\|_{H_{\infty}} = 1/\|g\|_{L_{\infty}} = 1/|g(j\omega_p)|
\]
and if only if \( n = 2 \) and
\[
\theta'_g(\omega_p) > |\sin(\theta_g(\omega_p))/\omega_p| . \tag{24}
\]

\textbf{Proof:} For the sake of readability, we postpone the full proof to Section VII-A.

Let us briefly explain the main idea behind the two stabilizability conditions (23) and (24). These conditions are obtained by applying Proposition 2 to the positive feedback system with loop transfer function \( L := g/f \). Due to the norm constraint on \( f \), the open-loop transfer function \( L \) must have peak gain \( \|L\|_{L_{\infty}} = 1 \) at frequency \( \omega_p \), which leads to condition (ii-a) of Proposition 2, and condition (19) is equivalent to \( \theta'_g(\omega_p) > 0 \). We can also see that condition (ii-b) does not hold. Hence, \( g \) is marginally stabilizable by some \( f \) when \( \theta'_g(\omega_p) \) is larger than the infimum of \( -\theta'_f(\omega_p) \) over the set of all suitable \( f \), given in (23) and (24).

More accurately, stabilizability conditions (23) and (24) emerge from the following PCR maximization problem:

\[
\sup f \in R1H_{\infty}, f(j\omega_p)g(j\omega_p) = 1 \text{ subject to } f(j\omega) = 1/\|g\|_{L_{\infty}} \forall \omega \in \mathbb{R}. \tag{25}
\]

We make the following claim.

\textbf{Claim:} The maximum of the PCR maximization problem (25) is equal to 0 when \( \omega_p = 0 \), and \(-|\sin(\theta_g(\omega_p))/\omega_p| \) when \( \omega_p \neq 0 \).

Section V is devoted to solving the PCR maximization problem (25) and proving the above claim; see Theorem 3. Meanwhile, several remarks on Theorem 1 are in order.

\textbf{Remark 1:} Note that the norm constraint on \( f \) implies that the loop transfer function \( L \) has a single peak gain at \( \omega_p \). Therefore, the marginal stability stated in Theorem 1 is single mode. That is, there is only one “marginally stable” pole (at the origin) for case (I), and a pair of “marginally stable” poles (at \( \pm j\omega_p \)) for case (II).

\textbf{Remark 2:} Note that \( \sin(\theta_g(\omega))/\omega \rightarrow \theta'_g(0) \) as \( \omega \rightarrow 0 \). Therefore, inequality (23) is not simply the limiting case of inequality (24).

\textbf{Remark 3:} For \( g \in G_n^0 \) or \( G_n^m \) with \( n \geq 3 \), it may be possible to find a stable \( f \) with \( \|f\|_{H_{\infty}} = 1/\|g\|_{L_{\infty}} \), such that all poles of the feedback system are in the CLHP. However, since the loop transfer function \( L \) has a single peak gain as a result of the norm constraint on \( f \), the poles on the imaginary axis must be located at \( 0 \) or \( \pm j\omega_p \), and hence, must have multiplicity larger than one. In such cases, the closed-loop system is polynomially unstable.

\section{Conditions for Exact RIR}

Based on Theorem 1 and Proposition 1, conditions for attaining the RIR of a system exactly given by the small gain condition are derived. Moreover, we also show that for some systems, their RIR’s are not given by the small gain condition. 

\textbf{Theorem 2:} 

(I) (Necessity) Let \( g \in G_n^0 := G_n^0 \cup G_n^m \) for some positive integer \( n \), and \( \omega_p \) be its peak-gain frequency. Define
\[
\mu_g(\omega_p) := \begin{cases} 0 & \text{if } \omega_p = 0 \\ |\sin(\theta_g(\omega_p))/\omega_p| & \text{otherwise}. \end{cases} \tag{26}
\]
If \( \mu_g(\omega_p) = 1/\|g\|_{L_{\infty}} \) and \( \theta'_g(\omega_p) \geq \mu_g(\omega_p) \).

(II) (Sufficiency) Let \( g \in G_n^0 \cup G_n^m \), and \( \omega_p \) be its peak-gain frequency. Then \( \mu_g(\omega_p) = 1/\|g\|_{L_{\infty}} \) if
\[
\theta'_g(\omega_p) > \mu_g(\omega_p) \tag{27}
\]
where \( \mu_g(\cdot) \) is defined in (26).

(III) Let \( g \in G_n^m \), where \( n \) is a positive odd integer. For such \( g \), we have \( \mu_g(\omega) > 1/\|g\|_{L_{\infty}} \).

\textbf{Proof:} See Section VII-B for a proof.

Several remarks are in order.

\textbf{Remark 4:} For \( g \in G_n^0 \cup G_n^m \), the gap between the necessary and the sufficient conditions is due to the cases where the exact RIR is attained through the polynomial instability. For example, consider the reduced-order model for the magnetic levitation system \( g_r(s) = k/(-s^2 + p^2) \) (see Section VI-B). One can readily verify that \( g_r \in G_1^0 \), \( \|g_r\|_{L_{\infty}} = |g_r(0)| = k/p^2 \), and \( \theta'_g(0) = 0 \). It is shown in [17, Sec. 3] that the exact RIR of \( g_r \) is \( 1/\|g\|_{L_{\infty}} \) and the critical controller results in a closed-loop system with double poles at the origin. This example shows that (27) is not necessary.

\textbf{Remark 5:} For \( g \in G_n^0 \) with \( n \geq 2 \), or \( g \in G_n^m \) with \( m \geq 2 \), the RIR of \( g \) may be given by the small gain condition. In these cases, one must find a critical controller with \( H_{\infty} \) norm equal to \( 1/\|g\|_{L_{\infty}} \), such that the closed-loop system has all its poles in the CLHP, and multiple poles at the origin (for \( g \in G_n^0 \)), or \( \pm j\omega_p \) (for \( g \in G_n^m \)). The reasoning for this fact is similar to that given in Remark 3.

\textbf{Remark 6:} For \( g \in G_1 \) or \( G_2 \) with multiple peak frequencies, it can be single mode marginally stabilized by some \( f \) with \( H_{\infty} \)-norm arbitrarily close to \( 1/\|g\|_{L_{\infty}} \), and hence has the exact RIR, if the following holds:
\begin{itemize}
  \item For \( g \in G_1 \), \( \|g(0)| = \|g\|_{L_{\infty}} \) and inequality (23) holds;
  \item For \( g \in G_2 \), there exists one peak frequency where inequality (24) holds.
\end{itemize}

For such \( g \), one can apply an inverse notch filter, which maintains the gain at the frequency where (23) or (24) holds and decreases the gain at all other frequencies by an appropriately small amount. This way, the filtered \( g \) has a unique peak frequency for which Theorems 1 and 2 become applicable. This in turn leads to the aforementioned results. For details, please refer to [18, Sec. 6].

\textbf{Example 1:} We here apply Theorem 2 to a class of second-order unstable systems \( g \in G \) represented by
\[
g(s) = 1/(s^2 + ps + q) : q \neq 0 \tag{28}
\]
to show the effectiveness of the results.

First, note that \( g \in G_1 \) if and only if \( q < 0 \); \( g \in G_2 \) if and only if \( q > 0 \), and \( p < 0 \). Also, note that \( |g(j\omega + \theta)|^2 := 1/D_\nu(\Omega) \),
where $\Omega := \omega^2$

$$D_2(\Omega) := (\Omega^2 + (p^2 - 2q)\Omega + q^2) + 2p(\Omega + q)\epsilon + o(\epsilon)$$

and $o(\epsilon)$ represents the terms with $\epsilon$ of second or higher orders. The peak gain frequency $\omega_p$ of $g$ can be found by minimizing $D_0(\Omega)$ subject to the constraint $\Omega \in [0, \infty)$. One can readily verify that the minimum of $D_0(\Omega)$ occurs at $\Omega_p := q - p^2/2$ when $q \geq p^2/2$, and at $\Omega_p = 0$ otherwise. Thus, we conclude that

- For any $g \in G_1$, $\omega_p = 0$ because $q - p^2/2$ must be negative; i.e., $g \in G_1$ implies $g \not\in G_0$
- For any $g \in G_2$, $\omega_p = 0$ when $2q \leq p^2$; otherwise, $\omega_p > 0$ and $\omega_p^2 = q - p^2/2$.

Now, the $\sigma$-gain CR can be calculated based on the form of (13). One can verify that

$$M'_g(\Omega) = -p(\Omega + q)/(\Omega^2 + (p^2 - 2q)\Omega + q^2) \quad (29)$$

and we have $M'_g(0) = -p/q$ and $M'_g(\Omega_p) = -2/p$. Applying Theorem 2, we have the following results:

(I) Suppose $g \in G_1$, i.e., $q < 0$. Then, $\rho_\sigma = \rho_\alpha := |1/|g(0)|| = |g(0)|$ holds if and only if $p \geq 0$.

(II) For any $g \in G_2$, i.e., $p < 0$, $2q > p^2 > 0$, we have $\rho_\sigma = \rho_p := 1/|g|_{L_\infty} = 1/|g(j\omega_p)|$, where $\omega_p^2 = \Omega_p = q - p^2/2$.

The proofs of the results (I) and (II) are as follows. Regarding (I), $p \geq 0$ is equivalent to $M'_g(0) = -p/q \geq 0$. Although statement (I) of Theorem 2 only gives the necessity for $p = 0$, we can readily show that a constant $\delta$ marginally stabilizes even for $p = 0$, which gives rise to the sufficiency. This completes the proof of (I). We compare the values of $|\sin(\theta_g(\omega))|/|\omega_p|$ with $-2/p$ to show (II). We can show that $|\sin(\theta_g(\omega))|/|\omega_p|^2 = 4/(4q - p^2) < 4/p^2 = M'_g(\Omega_p)^2$, since $2q > p^2$ is equivalent to $4q - p^2 > p^2$. This completes the proof of (II).

For $g \in G_2$, i.e., the case where $p < 0$, $0 < 2q \leq p^2$, we do not yet know whether $g$ has the exact RIR.

V. SUPREMIUM OF PCR OVER STABLE TRANSFER FUNCTIONS

In this section, the PCR maximization problem (25) is solved and the claim stated in the previous section is proven. It will be shown that the supremums are attained by the zeroth-order and the first-order all-pass functions for $\omega_p = 0$ and $\omega_p \neq 0$, respectively.

A. PCR Maximization

To solve the optimization problem described in (25) for $\omega_p \geq 0$, notice that the constraint $g(j\omega_p)f(j\omega_p) = 1$ is equivalent to the gain and phase conditions

$$A_f(\omega_p) \cdot A_g(\omega_p) = 0, \quad \theta_f(\omega_p) + \theta_g(\omega_p) = 0. \quad (30)$$

Also, notice that the phase variation $\theta_f(\omega)$ of a function $f$ is invariant to a constant scaling on $f$. Therefore, the essential aspects of the constraints in (25) are the phase of $f$ at $\omega_p$, and that $f$ attains its $\mathcal{H}_\infty$-norm at $\omega_p$. The magnitude of $f$ at $\omega_p$ is immaterial because the first equation in (30) can always be satisfied via a constant scaling on $f$. As such, without loss of generality, we will assume that the functions under consideration in this section have unit norm. To facilitate development, let us introduce two classes of transfer functions $f(s)$ based on its frequency response $f(j\omega) = |f(j\omega)|e^{j\theta_f(\omega)}$. Define

$$\mathcal{R}_F_{\omega_p, \theta_p} := \{ f \in \mathcal{R}_\mathcal{H}_\infty \mid 1 = ||f||_{\mathcal{H}_\infty} = |f(\omega_p)|, \quad \theta_f(\omega_p) = \theta_p \}.$$ 

This represents a class of proper real rational stable functions of which the $\mathcal{H}_\infty$-norm is attained at a specified frequency $\omega_p$ and the phase at that frequency is equal to a specified value $\theta_p$. Moreover, let us also consider

$$A_P(\omega_p, \theta_p) := A_P \cap \mathcal{R}_F_{\omega_p, \theta_p}$$

where $A_P := \{ f \in \mathcal{R}_\mathcal{H}_\infty \mid |f(j\omega)| = 1 \forall \omega \}$ is the set of all stable real rational all-pass functions with unit norm. Note that $A_P$ includes zeroth-order all-pass functions, which take values $\pm 1$ over the entire complex plane. Clearly, $A_P(\omega_p, \theta_p)$ is a subset of $A_P$ containing all-pass functions whose phase at $\omega_p$ is constrained to be a specified value $\theta_p$.

Using $\mathcal{R}_F_{\omega_p, \theta_p}$, we consider the following equivalent maximization problems of (25): [PCR maximization]

$$\sup_{f \in \mathcal{R}_F_{\omega_p, \theta_p}} M'_f(\omega_p) \equiv \sup_{f \in \mathcal{R}_F_{\omega_p, \theta_p}} M'_f(\omega_p). \quad (31)$$

The equivalence of the two problems follows straightforwardly from Lemma 2. Also, note that not only the two problems have the same supremum, but the arguments of supremum are also identical.

To solve (31) (with $-\theta_g(\omega_p)$ replaced by $\theta_p$, for notational simplicity), we will show that the supremum of $\theta'_f(\omega_p)$ and $M'_f(\omega_p)$ over $\mathcal{R}_F_{\omega_p, \theta_p}$ is in fact the same as that over $A_P(\omega_p, \theta_p)$.

This follows from a key observation that the minimum-phase factor of a stable function does not “help” in elevating the PCR at the peak frequency. To this end, let us consider the following problem whose solution is a lower bound for (31):

$$\sup_{f \in A_P(\omega_p, \theta_p)} \theta'_f(\omega_p) \equiv \sup_{f \in A_P(\omega_p, \theta_p)} M'_f(\omega_p). \quad (32)$$

Proposition 3: Consider the optimization problem (32).

(I) For $\omega_p = 0$, we must have $\theta_p \in \{0, \pi\} \mod 2\pi$. In this case,

$$\sup_{f \in A_P(\omega_p, \theta_p)} \theta'_f(\omega_p) = \sup_{f \in A_P(\omega_p, \theta_p)} M'_f(\omega_p) = 0. \quad (33)$$

The supremum is attained by $f(s) = 1$ or $f(s) = -1$.

(II) For $\omega_p \neq 0$ and $\theta_p \in (-\pi, \pi) \mod 2\pi$, we have

$$\sup_{f \in A_P(\omega_p, \theta_p)} \theta'_f(\omega_p) = \sup_{f \in A_P(\omega_p, \theta_p)} M'_f(\omega_p) = -\frac{\sin(\theta_p)}{\omega_p}. \quad (33)$$

Moreover, when $\theta_p \not\in \{0, \pi\}$, the supremum is attained by the first-order all-pass function of the form $f(s) = \frac{a_1}{\omega_p + a_2}$ or $f(s) = \frac{a_1}{\omega_p + a_2}$ satisfying the phase constraint $\theta'_f(\omega_p) = \theta_p$. When $\theta_p \in \{0, \pi\}$, the supremum is attained by a zeroth-order all-pass functions; i,e., $f(s) = 1$ or $f(s) = -1$. 

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Furthermore, the key observation that leads to the solution of (31) can be formulated as follows.

**Proposition 4:** Optimization problems (31) and (32) have the same solutions. That is

\[
\sup_{f \in \mathcal{F}_{\omega_p, \theta_p}} \theta_f'(\omega_p) = \sup_{f \in \mathcal{F}_{\omega_p, \theta_p}} \theta_f'(\omega_p).
\]  

(34)

Proofs of Propositions 3 and 4 can be found in Sections VII-C and VII-D, respectively. With these two propositions, we arrive at the main result of this section.

**Theorem 3:** Consider the optimization problem (31).

(i) For \(\omega_p = 0\), we must have \(\theta_p \in \{0, \pi\} \mod 2\pi\). In this case,

\[
\sup_{f \in \mathcal{F}_{\omega_p, \theta_p}} \theta_f'(\omega_p) = 0.
\]  

(35)

(ii) For \(\omega_p \neq 0\) and \(\theta_p \in (-\pi, \pi) \mod 2\pi\), we have

\[
\sup_{f \in \mathcal{F}_{\omega_p, \theta_p}} \theta_f'(\omega_p) = -|\sin(\theta_p)/\omega_p|.
\]  

(36)

Moreover, the supremum is attained by \(f(s) = 1\) or \(f(s) = -1\) when it is zero. When the supremum is not zero, it is attained by a first-order all-pass function as described in statement (II) of Proposition 3.

**Proof:** The result follows from Propositions 3 and 4 in a straightforward manner.

One may find the results in Proposition 3 and Theorem 3 somewhat counter-intuitive, as one may think a higher order all-pass function would give better result due to more optimizable parameters it provides. This additional “freedom” is not useful because of the constraint on the phase at \(\omega_p\). To better understand this point, let us consider the PCR of a generic second-order all-pass function with that of the first-order.

**Example 2:** We here evaluate the PCR of the second-order all-pass function

\[
f(s) := \frac{a - bs + s^2}{a + bs + s^2}, \quad a, b > 0.
\]

Since the phase and the \(\sigma\)-gain CRs are the same, we calculate the latter instead. For given \(\theta_p\) and \(\omega_p\), the phase constraint \(\theta_f'(\omega_p) = \theta_p\) requires that the parameters \(a\) and \(b\) be chosen so that

\[
\sin(\theta_p) = -\frac{2(a - \omega_p^2)b\omega_p}{(a - \omega_p^2)^2 + b^2\omega_p^2}.
\]  

(37)

holds. Furthermore, one can verify that

\[
M_f'(\omega) = -\frac{2(a - \omega^2)b}{(a - \omega^2)^2 + b^2\omega^2} - \frac{4\omega b}{(a - \omega^2)^2 + b^2\omega^2}.
\]  

(38)

For \(\omega_p \neq 0\), substituting (37) into equation (38) yields

\[
M_f'(\omega_p) = \sin(\theta_p)/\omega_p + \frac{2\omega_p^2}{a - \omega_p^2} \sin(\theta_p)/\omega_p.
\]  

(39)

Suppose \(\sin(\theta_p) = 0\). This implies \(a - \omega_p^2 = 0\), and (38) implies \(M_f'(\omega_p) < 0\). If \(\sin(\theta_p)/\omega_p \neq 0\), then \(a - \omega_p^2 > 0\) and clearly (39) implies \(M_f'(\omega_p) < -|\sin(\theta_p)/\omega_p|\). Finally, \(M_f'(\omega_p) < -|\sin(\theta_p)/\omega_p|\) also holds when \(\sin(\theta_p)/\omega_p > 0\).

To see this, note that in this case \(a - \omega_p^2 < 0\) and one can verify that

\[
1 + 2\omega_p^2/(a - \omega_p^2) < -1.
\]

Thus, we conclude that the best first-order all-pass function is better than any second-order one, as the PCR of the first-order all-pass function with the same constraint is equal to \(-|\sin(\theta_p)/\omega_p|\).

**VI. PRACTICAL APPLICATIONS**

In this section, we apply our main results to analyze (in)stability properties of system models that are derived from real-world applications. Section VI-A is concerned with exact robust instability analysis for a biological network oscillator called “repressilator,” of which the linearized model used is in \(\mathcal{G}_{ZF}^2\). Section VI-B is about digital stable controller synthesis for a magnetic levitation system, where the model belongs to \(\mathcal{G}_{ZF}^2\). The goal is to illustrate that our theoretical results are applicable to problems of significance to provide useful information. Note that the problem settings here are more practical than those considered in [17].

**A. Robust Instability Analysis for Repressilator**

Consider the repressilator with three dynamical units in a cyclic loop [5]. Its linearized model around an equilibrium state is approximated by a positive feedback system with loop-transfer function represented by

\[
h_e(s) = \frac{-k_e D^T(s)}{(s + \alpha_1)(s + \alpha_2)(s + \alpha_3)}
\]

where \(k_e > 0\) depends on the equilibrium state of the original nonlinear system [8] and \(D^T(s)\) denotes a Padé approximation of the time-delay transfer function \(e^{-\tau s}\). The nominal system with the characteristic equation \(1 = h_e(s)\) is assumed to be exponentially unstable. The subscript \(e\) is used to indicate that the quantity \(e\) depends on the equilibrium state, which is subject to the dc-gain of the uncertainty \(\delta(s)\) denoted by \(e := \delta(0)\). For more details about the repressilator model, see [8].

We are interested in assessing robust instability against a ball type multiplicative perturbation with a frequency weight function \(w_m(s) := (1 + \zeta T_m s)/(1 + T_m s)\). As explained at the beginning of Section II, the corresponding characteristic equation is \(1 - \delta(s)g_e(s) = 0\), where \(g_e(s) = w_m(s)h_e(s)/(1 - h_e(s))\). We set the parameters of the nominal system to be the same as in [8], i.e., \(\alpha_1 = 0.4621, \alpha_2 = 0.5545, \) and \(\alpha_3 = 0.3697\), and the fifth-order Padé approximation is used for the delay with \(\tau = 0.25\), which mainly accounts for maturation time of protein. The weight function \(w_m(s)\) is defined with \(T_m = 0.3\) and \(\zeta = 10\).

Since \(g_e\) is parameterized by the DC-gain of its stabilizing perturbation \(\delta\), obtaining its instability margin requires a more elaborated analysis. For a given \(e\), we apply Lemma 4 of [8] to verify whether \(g_e\) has the exact RIR equal to \(1/\|g_e\|_{\infty}\). According to the lemma, it is so if the following conditions hold:

(a) \(|e| < 1/\|g_e\|_{\infty}\); (b) \(g_e\) has even number of ORHP poles; and (c) \(g_e\) can be marginally stabilized by a stable perturbation \(\delta\) with \(\|\delta\|_{\mathcal{H}_\infty} = 1/\|g_e\|_{\infty}\). Numerical computations show that (a) holds for \(e \in (-0.193, 0.174) =: I_1\) and that \(g_e(s) \in \mathcal{G}_{ZF}^2\), which implies that (b) is satisfied for \(e \in [-0.94, 1) =: I_2\). Thus, \(1/\|g_e\|_{\infty}\) gives the exact RIR for the interval \(I_1 \cap I_2 = (-0.193, 0.174)\) if (c) is satisfied. Condition (c) can be readily verified by the PCR condition (27) stated in Theorem 2 and it,
is used for simplicity to avoid the complicated formulae. This is reasonable in practice since $\tau^{-1} \gg p$ typically holds, and hence, we may neglect the factor $(\tau s + 1)$ for control design purpose.

The first step is to derive the discretized plant model $g_d(z)$, where we assume that an ideal sampler and a synchronized zeroth-order hold with the sampling period $T > 0$ are placed around the continuous-time plant $g_c(z)$. The discretized model with one sample computational time delay $(1/z)$ is given by

$$g_d(z) = 2\kappa \{z + 1\}/((z - e^{-pT})(z - e^{pT}))$$  \hfill (43)$$

where $\kappa := k(1 - e^{-pT})(1 - e^{-pT})/(2p^2)$. Note that the static gain is preserved, i.e., $g_d(1) = g_r(0) = k/p^2$.

Our theoretical results in the continuous-time setting can be applied to discrete-time systems by introducing a bilinear transformation $z \leftarrow (1+s)/(1-s)$. In particular, a continuous-time equivalent of $g_d(z)$, denoted by $g_{d,c}(s)$, can be derived as follows:

$$g_{d,c}(s) = k_{c} \frac{(s - 1)^2}{(s - q)(s + q)(s + 1)}$$

where $k_c := 2\kappa/(1 - e^{-pT})(1 - e^{-pT})$. Note that $k_c$ can also be expressed as $k_c = -kq^2/p^2$. Therefore, we have $g_d(0) = k/p^2 = g_r(0)$, which is also equal to $|g_d(1)| = ||g_d||_{L_\infty}$. This is simply because the bilinear transformation preserves the gain of the corresponding frequency. It is also noticed that the unstable pole at $s = q$ is in the interval (0,1), implying that it is located to the left of the nonminimum-phase zero at $s = 1$, and hence, the PIP condition holds.

One can readily verify that $g_{d,c}(s) \in G_0^p$ and $\theta_{d,c}(0) < 0$. To see this, note that $A'_{g_{d,c}}(\omega)$ and $\theta'_{g_{d,c}}(\omega)$ are the real and imaginary parts of $\frac{d}{d\omega} \log g_{d,c}(j\omega)$, respectively. They are expressed as follows:

$$A'_{g_{d,c}}(\omega) = -\omega^2 - 2 - q^2$$

$$\theta'_{g_{d,c}}(\omega) = \frac{-3}{\omega^2 + 1}$$

By these expressions, we have $A'_{d,c}(0) \leq 0$, $A'_{d,c}(\omega) < 0 \forall \omega > 0$, and $\theta'_{d,c}(0) = -3$. Thus, by Theorem 2, we conclude that

$$\inf_{c \in G_0^p} ||c||_{H_\infty} > 1/||g_{d,c}||_{L_\infty} = 1/||g_d(0)|| = p^2/k$$

since the necessary condition for $d_c$ to have the exact RIR is violated. This, in turn, implies that the norm of the minimum-norm strongly stabilizing controller for $g_d$ must also be larger than $p^2/k = 1/||g_{d,c}||_{L_\infty}$.

To obtain an upper bound on $\inf_{c \in G_0^p} ||c||_{H_\infty}$ (which is also an upper bound on the norm of the minimum-norm strongly stabilizing controller for $g_d$), let us apply the lead compensator of the form $(b\ell + 1)/(a\ell + 1)$ where $m \geq 1$ is an integer and $b > a > 0$. The values of these parameters are to be chosen later. Let $\tilde{g}_{d,c}(s) := g_{d,c}(s)f(x)$. One can readily verify that

$$\theta'_{d,c}(\omega) = \theta'_{d,c}(\omega) + m \cdot \frac{(a - b)ab\omega^2 + (b - a)}{(b^2\omega^2 + 1)(a^2\omega^2 + 1)}$$

$$A'_{d,c}(\omega) = A'_{d,c}(\omega) + m \cdot \frac{-\omega^2 - a^2}{(b^2\omega^2 + 1)(a^2\omega^2 + 1)}.$$
Thus, for $\theta_{\tilde{g}_{dc}}'(0) = -3 + m(b - a) > 0$, we set $b = a + 3/m$, where $3r := 3 + \epsilon$, and $\epsilon > 0$ is arbitrarily small. With this selection of $b$, $\theta_{\tilde{g}_{dc}}'(0) > 0$ and $A'_{\tilde{g}_{dc}}(0) = 0$ regardless of the value of $a$. Furthermore, with $b = a + 3/m$, it can be verified that $A'_{\tilde{g}_{dc}}(\omega) \leq 0$ when $\omega \to 0^+$ if and only if $a \leq \frac{1}{2}(1/q^2 - 2/m + 1/2) =: a$. The condition also implies that $A'_{\tilde{g}_{dc}}(\omega) \leq 0 \forall \omega \geq 0$. Thus, $\tilde{g}_{dc}$ belongs to $\mathcal{G}_Q^+$ with positive PCR at the zero frequency for any $a$ satisfying $0 < a \leq \bar{a}$. Note that the upper bound $\bar{a}$ is positive if $m$ is sufficiently large, since $1/q^2$ is larger than 1. Applying Theorem 2, we have

$$\inf_{c \in \mathcal{G}(\tilde{g}_{dc})} \|c\|_{H_\infty} = 1/\|\tilde{g}_{dc}\|_{L_\infty} = 1/\|\tilde{g}_{dc}(0)\| = p^2/k.$$ 

Suppose $c^*$ is a (minimum-norm) strongly stabilizing controller for $\tilde{g}_{dc}$. Then, $c^*f$ is a strongly stabilizing controller for $g_{dc}$, and therefore, $\|c^*f\|_{L_\infty} \approx (p^2/k)(1 + 3/(ma))$ is an upper bound on $\inf_{c \in \mathcal{G}(g_{dc})} \|c\|_{L_\infty}$. To minimize the upper bound, we shall choose $a = \bar{a}$, which results in

$$1 < \inf_{c \in \mathcal{G}(g_{dc})} \|c\|_{L_\infty} \leq \left(1 + \frac{2q^2 \cdot 3^2}{m(2 - \frac{3^2}{m} + 1/q^2)}\right).$$

As a final remark, recall that $g := (1 - e^{-pT})/(1 + e^{pT})$, which is a monotonically increasing function of $pT$, and takes 0 value when $pT = 0$. As such, we see that the upper bound approaches the lower bound as $pT \to 0$; i.e., when the sampling is arbitrarily fast, we recover the continuous-time result, which is expected. Furthermore, for a given $pT$, one can try to minimize the upper bound over $m$ under the constraint $a > 0$; i.e., $m$ is a positive integer satisfying $m > q^2 \cdot 3^2/(2 - q^2)$. 

### VII. PROOFS OF MAIN RESULTS

#### A. Proof of Theorem 1

The arguments for proving both statements are similar. Here we will focus on the derivation for statement (II), and then, point to key differences that lead to statement (I).

We start with proving the sufficiency part of statement (II). Let $g \in \mathcal{G}_L^+$. Suppose $n = 2$ and (24) holds. For the case $\sin(\theta_g(\omega_p)) = 0$, let $f$ be the constant function with real value $1/j(\omega_p)$ and $L = g$. As $g \in \mathcal{G}_L^+$, we see that $L \in \mathcal{G}_L^+$, and $|L(j\omega)| < L(j\omega_p)$ for all $\omega \neq \pm \omega_p$. Furthermore, since $\theta_g'(\omega_p) = \theta_g'(\omega_p) + \theta_g'(\omega_p) = \theta_g'(\omega_p) > 0$, we also have $\frac{\partial}{\partial \omega} L(s)|_{s=j\omega_p} \neq 0$. Thus, (17) and condition (i) of Proposition 2 hold with $\omega_c = \omega_p > 0$. Lastly, since $|L(j\omega)| \leq 1$ for all $\omega$, we see that $0 = \nu_c(0) = 2 - 2$ with $\theta_g'(\omega_p) > 0$, and hence, condition (ii-a) of Proposition 2 also holds. By Proposition 2, we have that $f$ marginally stabilizes $g$. For the case $\sin(\theta_g(\omega_p)) = 0$, let

$$f(s) = \begin{cases} \frac{1}{g(\omega_p)} & \text{if } \theta_g'(\omega_p) \bmod 2\pi \in (0, \pi) \\ \frac{1}{g(\omega_p)} & \text{if } \theta_g'(\omega_p) \bmod 2\pi \in (-\pi, 0) \end{cases}$$

where $a > 0$ is chosen, such that $\theta_g'(\omega_p) + \theta_g'(\omega_p) = 0 \pmod{2\pi}$. Specifically, $a = \omega_p \tan(-\theta_g'(\omega_p)/2)$ when $\theta_g'(\omega_p) \pmod{2\pi} \in (0, \pi)$, and $a = \omega_p \tan(\theta_g'(\omega_p)/2)$ when $\theta_g'(\omega_p) \pmod{2\pi} \in (-\pi, 0)$. Since $f$ is an all-pass function satisfying $g(\omega_p)f(j\omega_p) = 1$, the loop transfer function $L$ satisfies $|L(j\omega)| < L(j\omega_p)$ for all $\omega \neq \pm \omega_p$. Furthermore, one can verify that for a given $\omega \neq 0$, $\theta_g'(j\omega) = -\sin(\theta_g(\omega))/\omega$. Thus, we again have $\theta_g'(\omega_p) = \theta_g'(\omega_p) + \theta_g'(\omega_p) > 0$ by (24). Therefore, the same arguments apply and we conclude that $f$ marginally stabilizes $g$ and the feedback system has a pair of single poles at $\pm j\omega_p$. Note that in both cases, the feedback system is $\omega_p$-marginally stable and the stabilizing (sub)system $f$ is stable and satisfies $|f|_{H_\infty} = 1/\|g\|_{L_\infty}$.

We note that the PCR condition (24) [respectively, (23)] for case (I) renders $\frac{\partial}{\partial \omega} L(s)|_{s=j\omega_p} \neq 0$, which in turn implies that the closed-loop poles at $\pm j\omega_p$ [respectively, at the origin for case (I)] must be simple.

For the necessity part of statement (II), let $g \in \mathcal{G}_L^+$ for which the peak gain of $g$ occurs at $\omega_p$. Let $f$ be the stable system that satisfies $|f|_{H_\infty} = 1/\|g\|_{L_\infty}$ and marginally stabilizes $g$. Since the feedback system is marginally stable and the loop transfer function $L := g f$ satisfies $\|g\|_{L_\infty} = \|g\|_{L_\infty} \leq 1$, we must have $|L(j\omega)| = 1$ for some frequency. This can only occur when $f$ satisfies $1/\|g\|_{L_\infty} = \|g\|_{L_\infty} \geq |f(j\omega)|$ for any $\omega \neq \pm \omega_p$, which in turn implies that $|L|_{L_\infty} = |g|_{L_\infty} > |L(j\omega)| \forall \omega \neq \pm \omega_p$. Since $f$ is stable, we have $L \in \mathcal{G}_L^+$ with peak gain occurring at $\omega_p$ and equal to 1. This further implies that the feedback system must be $\omega_p$-marginally stable. By Proposition 2, $L$ must satisfy condition (ii-a) or condition (ii-b). Note that $|L|_{L_\infty} \leq 1$ implies that $\nu_c(0) = 0$ and condition (ii-b) can never be satisfied. Thus, condition (ii-a) must hold and we conclude that $n = 2$ as the corresponding $\omega_c$ is equal to $\omega_p$, which is strictly larger than 0. Moreover, the necessary condition $\theta_g'(\omega_p) > 0$ implies $\theta_g'(\omega_p) > -\theta_g'(0)$. Inequality (24) emerges as one finds the infimum of $-\theta_g'(\omega_p)$ over the set of all suitable $f$’s. This results in the optimization problem we stated in (25), and the claim thereafter gives condition (24).

Regarding statement (I), we note that the statement deals with the special case, where $\omega_p = 0$; hence, its proof is almost identical to that of statement (II). For sufficiency, notice that since $g(0)$ is real, the arguments for the case where $\sin(\theta_g(\omega_p)) = 0$ apply. The marginally stabilizing $f$ is equal to $1/\|g(0)\$. The remaining arguments are identical, except when we verify condition (ii-a) of Proposition 2, we have the corresponding $\omega_c = 0$ and $n = 1$. For necessity, again, the same arguments for proving the necessity part of statement (II) apply. As such, condition (ii-a) of Lemma 4 implies that $n = 1$, and $\theta_g'(0)$ must satisfy $\theta_g'(0) > -\theta_g'(0)$. Inequality (23) emerges as the infimum of the right-hand side is equal to 0, as we have stated and has been shown in Section V.

#### B. Proof of Theorem 2

To prove statement (I), we need the following lemma, whose proof is given in Appendix D.

**Lemma 5:** Given $\omega_c \geq 0$, an integer $n \geq 1$, and a transfer function $L \in \mathcal{G}_n$, consider the positive feedback system with loop transfer function $L$ satisfying the following condition:

$$1 = \|L(j\omega_c)| = \|L\|_{L_\infty}$$

$$|L(j\omega)| < |L(j\omega)| \forall \omega \neq \pm \omega_c.$$  

(45)

If the closed-loop system has all its poles in the CLHP, then, $\theta_L'(\omega_c) \geq 0$.
Now suppose \( g \in G_0^{n} \) has the exact RIR equal to \( 1/\|g\|_{L_{\infty}} \). This implies that one can find a stable \( f \), \( \|f\|_{H_\infty} = 1/\|g\|_{L_{\infty}} \), such that the closed-loop system, with loop transfer function \( L := gf \), has all its poles in the CLHP. Note that \( \|L\|_{L_{\infty}} \leq 1 \); therefore, \( L \) must satisfy (45) with \( \omega_c = 0 \), whereby \( \theta'_{f}(0) = \theta'_{g}(0) + \theta'_{f}(0) \geq 0 \). This implies \( \theta'_{g}(0) \geq -\theta'_{f}(0) \), and hence, \( \theta'_{g}(0) \geq 0 \) as the infimum of the right-hand side is equal to 0, which is stated in the proof of Theorem 1 and has been shown in Section V. The arguments for \( g \in G_0^{\#} \) are identical, except that in this case we have \( \omega_c := \omega_p > 0 \), so the right-hand side of (43) is set to 0. The factorization of \( M_{\theta}^{*} \) can be found by searching over the subset of \( \mathcal{F}_{\theta}^{\#} \) that contains real-rational all-pass functions, which are constant functions or can be factored as products of first-order factors. Furthermore, among these all-pass functions, Equation 8 shows that

\[
M_f^{\#}(\omega_p) \leq -\left( \frac{\sin(\theta_f(\omega_p))}{{\omega}_p}\right) = -\left( \frac{\sin(\theta_f)}{{\omega}_p}\right) \leq 0.
\]

When \( \theta_f \notin \{0, \pi\} \), the supremum is attained by first-order all-pass function in the form of \( \frac{a-\pi}{a+\pi} \). The value of \( a > 0 \) is chosen, such that \( \sin(\theta_f) = \frac{\sin(\theta_f)}{a-\pi} = \frac{\sin(\theta_f)}{a+\pi} \). One can readily verify that such an always exists. When \( \theta_f \in \{0, \pi\} \), it is clear that \( f(s) = 1 \) or \( f(s) = -1 \) would satisfy the angular constraint and attain the supremum of the PCR, which is equal to 0.

For the case where \( \omega_p = 0 \), first we note that, since we consider real rational function \( f \), \( f(0) \) is necessarily real, and thus \( \theta_f(0) \) can only assume value 0 or \( \pi \) (mod 2\( \pi \)). Since \( M_f^{\#}(\cdot) \) by Lemma 4, without loss of generality we can consider only all-pass functions \( f \), such that \( f(0) > 0 \); i.e., the corresponding \( \theta_f \) is set to 0. The factorization of \( f \) implies that \( M_f(\cdot) = \sum_{j=1}^{n} M_f^{\#}(\cdot) \). Note that for a first-order factor of the form \( \frac{a-\pi}{a+\pi} \), the \( \sigma \)-gain CR at 0 is equal to \(-2/a \), whereas for a second-order factor of the form \( \frac{a-2\pi/b}{a+2\pi/b} \), the CR is \(-2/b \). Therefore, one concludes that \( M_f^{\#}(0) \) is strictly less than 0 if the order of \( f \) is larger than or equal to 1. Hence, the supremum of \( M_f^{\#}(\cdot) = \theta_f^{\#}(0) \) is equal to 0, obtained by the zeroth-order all-pass functions \( f(s) = 1 \) or \( f(s) = -1 \).

D. Proof of Proposition 4

To prove Proposition 4, we need the following lemma, which provides an upper bound for the PCR of any minimum-phase stable function at the peak-gain frequency.

\[ L_{\theta}(s) \in \mathcal{R}_{\theta}, \text{ suppose } \theta_f(\omega_p) = \left( -\pi, \pi \right), \text{ and } \|f(j\omega_p)\|_{H_{\infty}}. \] Then

\[
\theta_f^{\#}(\omega_p) \leq -\left( \frac{\sin(\theta_f(\omega_p))}{\omega_p}\right).
\]
Moreover, if $\omega_p = 0$, then $\theta'_f(\omega_p) \leq 0$.

The proof of Lemma 10 can be found in the appendix. To facilitate the development, let us also define

$$
\mathcal{O}_{\omega_p, \theta_p} := \{ f \in \mathcal{R}H_\infty : f \text{ is minimum-phase} \}
$$

$$
| f(j\omega_p) | = \| f \|_{H_\infty}, \text{ and } \theta_f(\omega_p) = \theta_p).
$$

First, consider the case where $\omega_p \neq 0$ and $\theta_p \in (-\pi, \pi]$. Since every $f \in \mathcal{R}H_\infty$ admits an inner–outer factorization $f = f_o f_o$ with $f_i \in \mathcal{R}H_\infty$ being all-pass and $f_o \in \mathcal{R}H_\infty$ being minimum-phase, it follows that $| f_o(j\omega_p) | = \| f_o \|_{H_\infty}$ and

$$
\sup_{f_o \in \mathcal{R}F_{\omega_p, \theta_p}} \theta'_f(\omega_p) = \sup_{f_o \in \mathcal{R}F_{\omega_p, \theta_p}} \left( \theta'_f(\omega_p) + \theta'_f(\omega_p) \right)
$$

$$
\leq \sup_{\theta \in (-\pi, \pi]} \left( \sup_{f_o \in \mathcal{R}F_{\omega_p, \theta}} \theta'_f(\omega_p) + \sup_{f_o \in \mathcal{R}F_{\omega_p, \theta}} \theta'_f(\omega_p) \right)
$$

$$
\leq \sup_{\theta \in (-\pi, \pi]} \left( \frac{| \sin(\theta) | - | \theta - \theta |}{| \omega_p |} \right) \leq \sin(\theta_p) \omega_p
$$

where the second inequality follows from Proposition 3 and Lemma 10, and the last inequality follows from the fact that $|b - a| + |\sin(a)| - |\sin(b)| \geq 0$ for all $a, b \in (-\pi, \pi]$. Lastly, since $|\sin(\theta)/|\omega_p| = \sup_{f \in \mathcal{R}F_{\omega_p, \theta_p}} \theta'_f(\omega_p) \leq \sup_{f \in \mathcal{R}F_{\omega_p, \theta_p}} \theta'_f(\omega_p)$, we conclude that the supremum of $\theta'_f(\omega_p)$ over $\mathcal{R}F_{\omega_p, \theta_p}$ is the same as that over $\mathcal{R}F_{\omega_p, \theta_p}$.

Now, consider the case where $\omega_p = 0$ and $\theta_p \in \{0, \pi\}$. The reason why the value of $\theta_p$ is restricted to 0 or $\pi$ is due to $f$ being real rational, and therefore, $\theta_f(\omega_p) \in \{0, \pi\}$. The rest of the derivation follows the same arguments. By the inner–outer factorization of $f$, we have

$$
\sup_{f \in \mathcal{R}F_{0, \theta_p}} \theta'_f(0) = \sup_{f = f_o f_o \in \mathcal{R}F_{0, \theta_p}} \left( \theta'_f(0) + \theta'_f(0) \right)
$$

$$
\leq \sup_{\theta \in (0, \pi]} \left( \theta'_f(0) + \theta'_f(0) \right)
$$

$$
\leq \sup_{\theta \in (0, \pi]} \theta'_f(0) = 0.
$$

The second inequality follows from Lemma 10, where it is shown that $\theta'_f(\omega_p) \leq 0$ for any minimum-phase $f_o \in \mathcal{R}H_\infty$.

The last equality follows from Proposition 3, which concludes the proof.

**VIII. CONCLUSION**

This article examined the exact RIR condition motivated by robust instability analysis against stable perturbations and minimum-norm strong stabilization. We have shown that the problem of finding the exact RIR may be turned into the problem of maximizing the PCR at the peak frequency with a phase constraint. It has been proven that the supremum is attained by a constant or a first-order all-pass function, which yields conditions for which we can find the exact RIR in terms of the PCR. Two practical applications have been provided to demonstrate the effectiveness of our theoretical results in practice.

**APPENDIX A PROOF OF LEMMA 3**

Given a minimum-phase function $f \in \mathcal{R}H_\infty$, let $h(s) := \frac{\log f(s)}{f(s)}$. Note that $h \in \mathcal{R}H_\infty$ and is strictly proper, and $h(j\omega) = \theta'_f(j\omega) - jA'_f(j\omega)$.

Now, let $k(s) := s \cdot h(s) \in \mathcal{R}H_\infty$. Then, we have

$$
k(j\omega) = j\omega h(j\omega) = \omega A'_f(j\omega) + j\omega \theta'_f(j\omega).
$$

Following the derivation in [21, Sec. 3] gives the integral formula for $\theta'_f(j\omega)$ stated in (15). Now rewrite the right-hand side of (15) as

$$
\lim_{\epsilon \to 0} \frac{2}{\pi} \int_0^\infty \frac{\omega A'_f(j\omega)}{\omega^2 - \omega_p^2} \omega + \int_{\omega_p+\epsilon}^\infty \frac{\omega A'_f(j\omega)}{\omega^2 - \omega_p^2} \omega d\omega.
$$

Applying integration by parts to the two terms in the parentheses yields

$$
\omega A_f(j\omega) \int_0^\infty \frac{\omega^2 - \omega_p^2}{\omega^2 - \omega_p^2} \omega + \int_{\omega_p+\epsilon}^\infty \frac{\omega^2 + \omega_p^2}{\omega^2 - \omega_p^2} \omega d\omega.
$$

Since

$$
\lim_{\omega \to 0} \omega A_f(j\omega) = \lim_{\omega \to \infty} \omega A_f(j\omega) = 0
$$

holds, the boundary terms become

$$
\frac{(\omega_p - \epsilon) A_f(j(\omega_p - \epsilon))}{\omega^2 - \omega_p^2} - (\omega_p + \epsilon) A_f(j(\omega_p + \epsilon))
$$

$$
= \frac{2\omega_p^2 - \epsilon^2}{\epsilon^2 - 4\omega_p^2} A_f(j(\omega_p - \epsilon)) + A_f(j(\omega_p + \epsilon))
$$

$$
+ \frac{\omega_p(A_f(j(\omega_p + \epsilon)) - A_f(j(\omega_p - \epsilon)))}{\epsilon^2 - 4\omega_p^2}.
$$

Note that $A_f(j(\omega_p) = 0$, and thus, by L’Hôpital’s rule we have

$$
\lim_{\epsilon \to 0} A_f(j(\omega_p - \epsilon)) + A_f(j(\omega_p + \epsilon))
$$

$$
= \lim_{\epsilon \to 0} \frac{A_f(j(\omega_p - \epsilon)) + A_f(j(\omega_p + \epsilon))}{\epsilon}
$$

$$
= 0
$$

which in turn implies that the boundary terms approach zero as $\epsilon \to 0$. Thus, we have

$$
\int_0^\infty \frac{\omega A'_f(j\omega)}{\omega^2 - \omega_p^2} \omega d\omega
$$

$$
= \lim_{\epsilon \to 0} \left( \int_0^{\omega_p - \epsilon} \frac{(\omega^2 + \omega_p^2)}{(\omega^2 - \omega_p^2)^2} A_f(j\omega) d\omega
$$

$$
+ \int_{\omega_p + \epsilon}^\infty \frac{(\omega^2 + \omega_p^2)}{(\omega^2 - \omega_p^2)^2} A_f(j\omega) d\omega
$$

$$
= \int_0^\infty \frac{(\omega^2 + \omega_p^2)}{(\omega^2 - \omega_p^2)^2} A_f(j\omega) d\omega
$$

as claimed in the second part of the lemma.
The idea for a proof of (i) is based on the Nyquist stability criterion, where a positive feedback system with unstable loop transfer function is stable if and only if the number of counter-clockwise encirclements by the Nyquist plot about 1 + j0 is equal to the number of open-loop poles in the ORHP, “n” in this case. The proof is trivial by considering the Nyquist plot of \( L(j\omega + \epsilon) \) with a sufficiently small positive number \( \epsilon > 0 \) instead of the original Nyquist plot of \( L(j\omega) \), so that any pole of the closed-loop system on the imaginary axis are placed outside of the Nyquist contour. Noting that \( L \) is a strictly proper \( R L_{\infty} \) function, the equivalence of (i) and (ii) follows from continuity and boundedness of \( L(j\omega + \epsilon) \) in addition to the property \( L(j\omega + \epsilon) \to 0 \) as \( \omega \to \pm \infty \).

It is clear that conditions (iii-a) and (iii-b) are necessary for marginal stability since they mean existence of simple roots of \( 1 + L(j\omega) = 0 \) on the imaginary axis. Conversely, condition (i) or (ii) implies that all the poles are in the CLHP, and hence, additional conditions (iii-a) and (iii-b) are sufficient for marginal stability.

First, note that the PCR at \( \omega = \omega_c \) cannot be equal to zero. The reason is as follows. Suppose \( \theta_L(\omega_c) = 0 \), then together with (17) this implies \( L'(j\omega_c) = 0 \), i.e., there are at least two feedback poles at \( j\omega_c \). Therefore, \( \theta'_L(\omega) \) cannot be 0. As such, the strict inequality conditions (19) and (20) can be equivalently replaced by \( \theta'_L(\omega) \geq 0 \) and \( \theta'_L(\omega) \leq 0 \), respectively. They will be treated as such when we prove the necessity of these two conditions.

Necessity: Condition (i) is necessary from the requirement on the closed-loop pole location on the imaginary axis for \( \omega_c \)-marginal stability. The necessity of condition (ii-a) or (ii-b) is derived from condition (ii) in Lemma 4, which is \( \nu_o(\epsilon) = n \) for sufficiently small \( \epsilon > 0 \).

When \( \omega_c > 0 \), condition (i) implies that there are two segments of the Nyquist plot of \( L(j\omega) \) passing through the critical point \( 1 + j0 \), which corresponds to the two different frequencies \( \pm \omega_c \). Moreover, we see that the two curves go across the real axis in the same direction since the Nyquist plot is symmetric about the real axis, i.e., \( L(j\omega) \) and \( L(-j\omega) \) are complex conjugate to each other for all \( \omega \in \mathbb{R} \). This means that the possible increment or decrement of \( \nu_o(\epsilon) \) for \( L(j\omega + \epsilon) \) are two when \( \epsilon \) is slightly perturbed away from zero. Hence, we have the following three possibilities: \( \nu_o(0) = n - 2, n, \) and \( n + 2 \). Note, that the first requirements of conditions (ii-a) and (ii-b) correspond to cases \( \nu_o(0) = n - 2 \) and \( \nu_o(0) = n \), respectively.

Let us first consider the case \( \nu_o(0) = n - 2 \), where the necessity of the second condition of (ii-a) can be shown by contradiction. Suppose the PCR is negative. Since \( \theta'_L(\omega) = M'_L(\omega) < 0 \), the Nyquist plot of \( L(j\omega + \epsilon) \) with small \( \epsilon > 0 \) crosses the real axis to the left of the critical point \( 1 + j0 \) in the downward direction as seen in the second row of the top figure of Fig. 1. This implies that \( \nu_+(\epsilon) \) and \( \nu_-(\epsilon) \) are constant for sufficiently small \( \epsilon \geq 0 \), and hence, \( \nu_o(\epsilon) = n - 2 \) is preserved for small \( \epsilon > 0 \).

This means violation of condition (ii) in Lemma 4, implying that the feedback system is not marginally stable. By contradiction, the necessity of the second condition (ii-a) is proved.

The idea for showing the necessity of condition (ii-b) for the case \( \nu_o(0) = n \) is the same as that of condition (ii-a), i.e., by contradiction. We assume that the PCR is positive, which yields that the Nyquist plot of \( L(j\omega + \epsilon) \) with small \( \epsilon > 0 \) passes through the real axis on the right of the critical point \( 1 + j0 \) in the upward direction as seen in the first row of the top figure of Fig. 1. This implies that \( \nu_+(\epsilon) \) increments by 2 and that \( \nu_(\epsilon) \) does not change when \( \epsilon \) is perturbed positively away from zero. Therefore, we have \( \nu_o(\epsilon) = n + 2 \) for sufficiently small \( \epsilon > 0 \), contradicting condition (ii) in Lemma 4, thus, the necessity of the second condition (ii-b) is proved.

It should be noticed that the case \( \nu_o(0) = n + 2 \) never happens, because the change of the number \( \nu_o(0) \neq \nu_o(\epsilon) \) with small perturbation \( \epsilon > 0 \) occurs only if the \( \sigma \)-gain CR \( M'_L(\omega) \) is nonnegative as seen in the first row of the top figure of Fig. 1, which always gives the increase of the number \( \nu_o(0) < \nu_o(\epsilon) = n \) due to the non-negativity of the PCR \( \theta'_L(\omega) \).

Finally, the proof for the case \( \omega_c = 0 \) is almost the same as that for \( \omega_c > 0 \). The only difference is the number of the Nyquist plot segments crossing the real axis at the critical point \( 1 + j0 \), which is one instead of two when \( \omega_c = 0 \). Other than this difference, the arguments above are still valid.

Sufficiency: The proof of the sufficiency is similar to that of the necessity, and hence, we only outline sufficiency of condition (ii-a). When the phase (or \( \sigma \)-gain) CR is positive, the Nyquist plot of \( L(j\omega + \epsilon) \) passes through the real axis on the right of the critical point \( 1 + j0 \) in the upward direction as shown in the first row of the top figure of Fig. 1. This implies that the number of crossing points on the real semi-interval \((1, +\infty)\) from the negative imaginary region to the positive imaginary region increases by one (respectively, two) for \( \omega_c = 0 \) (respectively, \( \omega_c > 0 \)). Hence, we have \( \nu_o(\epsilon) = n \) for sufficiently small \( \epsilon > 0 \), which guarantees the marginal stability due to Lemma 4.

Define \( \nu_o(\cdot) \) as in Proposition 2. Clearly, \( \nu_o(0) = 0 \) due to the fact that \( |L(j\omega)| \leq 1 \) for all \( \omega \). Suppose \( \theta'_L(\omega_c) < 0 \). By the arguments stated in Proposition 2, this would imply that \( \nu_o(\epsilon) = \nu_o(0) = 0 \) for sufficiently small positive \( \epsilon \), which in turn implies that the feedback system does not have all its poles in the CLHP by Lemma 4. Note that by Lemma 4, \( \nu_o(\epsilon) = n \) is needed for having all closed-loop poles in the CLHP.
Appendix F
Proof of Lemma 7

Let $k$ be a non-negative integer, such that $\theta_1 + \cdots + \theta_n + k\pi \in [-\pi, 0]$. Note that (47) is equivalent to
\[
sin \theta_1 + \cdots + \sin \theta_n \leq \sin(\theta_1 + \cdots + \theta_n + k\pi).
\] (50)

To see this, notice that the right-hand side is equal to $\sin(\theta_1 + \cdots + \theta_n)$ if $k$ is even, and $-\sin(\theta_1 + \cdots + \theta_n)$ if $k$ is odd. Since the right-hand side is always nonpositive given the range of $\theta_1 + \cdots + \theta_n + k\pi$, the right-hand side of (50) is equivalent to $-|\sin(\theta_1 + \cdots + \theta_n)|$. Given this, we will proceed to prove (50).

The claim can be proven by induction. The claim is obviously true when $n = 1$. Suppose, it is true for $i = 1, \ldots, n - 1$. With $n$ terms, we have $\sum_{i=1}^n \sin \theta_i \leq \sin \theta + \sin \theta_n$, where $\theta = \theta_1 + \cdots + \theta_{n-1} + m\pi$ for some $m$, such that $\theta \in [-\pi, 0)$. The rest of the proof boils down to analyzing three possible scenarios: both $\theta$ and $\theta_n$ belong to $[-\pi/2, 0]$, both $\theta$ and $\theta_n$ belong to $[-\pi, -\pi/2)$, and lastly, one is in $[-\pi/2, 0]$ and another is in $[-\pi, -\pi/2)$.

Suppose both $\theta$ and $\theta_n$ belong to $[-\pi/2, 0]$. Then, we have $\theta + \theta_n \in [-\pi, 0]$, and $\sin \theta + \sin \theta_n \leq \sin \theta \cos \theta_n + \sin \theta_n \cos \theta = \sin(\theta + \theta_n)$. The inequality holds because $\cos \theta_n, \cos \theta \in [0, 1]$ and $\sin \theta_n, \sin \theta \in [-1, 0]$. Thus, we conclude 
\[
\sum_{i=1}^n \sin \theta_i \leq \sin(\sum_{i=1}^n \theta_i + k\pi), \quad \text{where } k := m
\] and $\sum_{i=1}^n \theta_i + k\pi \in [-\pi, 0)$.

Now, suppose both $\theta$ and $\theta_n$ belong to $[-\pi, -\pi/2)$. We have $\theta + \theta_n \in [-2\pi, -\pi)$, and $\cos \theta_n, \cos \theta \in [-1, 0)$. This implies $\sin \theta + \sin \theta_n \leq \sin(-\cos \theta_n) + \sin(-\cos \theta) = -\sin(\theta + \theta_n) = \sin(\theta + \theta_n + \pi)$. Thus, we again conclude 
\[
\sum_{i=1}^n \sin \theta_i \leq \sin(\sum_{i=1}^n \theta_i + k\pi), \quad \text{where } k := m + 1
\] and $\sum_{i=1}^n \theta_i + k\pi \in [-\pi, 0)$.

Lastly, suppose without loss of generality that $\theta_n \in [-\pi/2, 0]$ and $\theta \in [-\pi, -\pi/2)$. This time, $\theta + \theta_n \in [-3\pi/2, -\pi/2)$. Depending on $\theta + \theta_n \in [-\pi, -\pi/2)$ or $\theta + \theta_n \in [-3\pi/2, -\pi)$, we apply arguments similar to those in the previous two paragraphs to conclude inequality (50). Note, that the inequality $\sin \theta + \sin \theta_n \leq \sin(\pm \cos \theta_n) + \sin(\pm \cos \theta)$ holds regardless of the signs of $\cos \theta$ and $\cos \theta_n$, because $\sin \theta, \sin \theta_n \leq 0$ and $\cos \theta, \cos \theta_n \in [-1, 1]$. This concludes the proof.

Appendix G
Proof of Lemma 8

In light of Lemma 6, we can consider only positive $\omega_p$ without loss of generality. Furthermore, as a consequence of results on finite Blaschke products [20], given an $n$th-order real-rational all-pass function $H$ with unit norm and only real poles, $H$ can be factored into $H(s) = cH_1(s) \cdots H_n(s)$, where $H_i(s) = \frac{a_i - s}{a_i + s}$ with $a_i > 0$, $i = 1, \ldots, n$, and $c \in \{-1, 1\}$.

First, consider $c = 1$. Let $\omega_p > 0$ and $\theta_i := \angle H_i(j\omega_p)$. One can readily verify that
\[
H_i(j\omega_p) = \frac{a_i - j\omega_p}{a_i + j\omega_p} = \frac{(a_i^2 - \omega_p^2) - j(2a_i \omega_p)}{a_i^2 + \omega_p^2} = \frac{a_i - j\omega_p}{a_i + j\omega_p}.
\]
and, therefore, $\sin \theta_i = \frac{-2a_i \omega_p}{a_i^2 + \omega_p^2} < 0$. This implies $\theta_i \in (-\pi, 0)$. Moreover, as $\|H_i\|_\infty = 1$, we have
\[
M'_H(\omega_p) = \sum_{i=1}^n M'_H(\omega_p) = \sum_{i=1}^n \frac{-2a_i}{\omega_p^2 + a_i^2} = \sum_{i=1}^n \sin \theta_i \omega_p.
\]
Thus,
\[
M'_H(\omega_p) \leq -|\sin(\theta_1 + \theta_2 + \cdots + \theta_n)| = -|\sin(\theta_H(\omega_p))| \omega_p
\]
where the inequality follows from Lemma 7 and $\omega_p > 0$, and the last equality follows from $\theta_H(j\omega_p) = \sum_{i=1}^n \theta_i$.

Next, consider $c = -1$. In this case we have
\[
M'_H(\omega_p) = M'_{-H}(\omega_p) \leq -|\sin(\theta_{-H}(\omega_p))|/\omega_p.
\]
Here, we use the fact that $\sin(\theta_{-H}(\omega_p)) = \sin(\theta_H(\omega_p))$. It is clear that the inequality (48) becomes equality if the order of $H$ is one. It is also clear that, for the zeroth-order all-pass functions $H(s) = 1$ and $H(s) = -1$, $M'_H(\omega_p) = 0$ and $\sin(\theta_H(\omega_p)) = 0$. So the equality also holds when the order of $H$ is zero.
where $\tilde{\gamma} = \frac{1}{2}(1 + \sqrt{1 - \gamma^2})$ and $\gamma = \frac{1}{2}(1 - \sqrt{1 - \gamma^2})$. Note that both $\tilde{\gamma}$ and $\gamma$ are positive. Thus, both $(a_r, b_r)$ and $(a_c, b_c)$ need to satisfy one of the following affine equations: $a = \omega_p^2 + \gamma \omega_p b$, and $a = \omega_p^2 + \gamma \omega_p b$. Moreover, for $\cos(\theta_H(\omega_p)) = \cos(\theta_H(\omega_p))$ to hold, $(a_r, b_r)$ and $(a_c, b_c)$ must satisfy the same affine equation, which then leads to $\theta_H(\omega_p) = \theta_H(\omega_p)$.

Now, suppose $(a_r, b_r)$ and $(a_c, b_c)$ satisfy $a = \omega_p^2 + \gamma \omega_p b$. The inequality $a_r \leq b_r^2/4$ implies that

$$
(\omega - b)^2 \geq 4(1 + \gamma^2) \omega_p^2
$$

which then leads to $a = \omega_p^2 + \gamma \omega_p b$. According to Theorem 1, we have $\omega_p^2(\frac{\omega}{\omega_p})^2 < 0$, and thus $\omega_p^2 + \gamma \omega_p b = 0$. Putting them together yields $a_r = \omega_p^2 > a_c^2 > 0$. In view of (51) and noting that $2\omega_p \sin(\theta_H(\omega_p)) = 2\omega_p \sin(\theta_H(\omega_p)) > 0$, we conclude that inequality (49) holds because the second term on the right-hand side of (51) is less negative for $H_r$. Apparently, the same arguments will hold if both $(a_r, b_r)$ and $(a_c, b_c)$ satisfy the other affine equation, as one simply replaces $\gamma$ by $\gamma$.

If $\omega_p$ is such that $a_c - \omega_p^2 < 0$, similar arguments will lead to inequality (49). In this case, $\gamma$ is not negative, and the affine equations derived from (53) are replaced by $a = \omega_p^2 - \gamma \omega_p b$ and $a = \omega_p^2 - \gamma \omega_p b$, where the forms of $\gamma$ and $\gamma$ are defined as those below (53), but with $\gamma$ replaced by $|\gamma|$. The inequalities for $a_r$ and $a_c$ [stated in (54)] become

$$
a_r - \omega_p^2 \leq -2\gamma + \sqrt{1 + \gamma^2} \omega_p^2 < 0, \quad 0 > a_c - \omega_p^2 \leq -2\gamma + \sqrt{1 + \gamma^2} \omega_p^2.
$$

Now, with $2\omega_p \sin(\theta_H(\omega_p)) = 2\omega_p \sin(\theta_H(\omega_p)) > 0$, we again have (49).

Finally, if $a_r - \omega_p^2 = 0$, we have $a_c - \omega_p^2 = 0$ and $M_r'((\omega_p)) = -4/b_r$, $M_c'((\omega_p)) = -4/b_r$. Again, we conclude inequality in (49) because $-4/b_r < -2\sqrt{\gamma} = -2\sqrt{\gamma} < -4/b_r$.

### APPENDIX I

**PROOF OF LEMMA 10**

As $\theta_f(\omega)$ and $\theta_f'(\omega)$ are both scale invariant, we can assume without loss of generality that $||f||_{H_\infty} = 1$. We proceed to show that

$$
|\omega_p| |\theta_f'(\omega_p)| \leq -|\theta_f(\omega_p)| = -\frac{2|\omega_p|}{\pi} \int_0^\infty \frac{A_f(\omega) - A_f(\omega_p)}{\omega^2 - \omega_p^2} \, d\omega.
$$

Since $||f||_{H_{\infty}} = 1$, we have $A_f(\omega) \leq 0$ for all $\omega \in \mathbb{R}$ and $A_f(\omega_p) = 0$. Suppose $\omega_p \neq 0$. By Lemma 3, we have

$$
|\omega_p| |\theta_f'(\omega_p)| = \frac{2|\omega_p|}{\pi} \int_0^\infty \frac{A_f(\omega) \omega^2 + \omega_p^2}{(\omega^2 - \omega_p^2)^2} \, d\omega.
$$

Since $\omega^2 + \omega_p^2 \geq \frac{1}{|\omega - \omega_p|^2}$ for $\omega \in [0, \omega_p] \cup (\omega_p, \infty)$, it follows

$$
|\omega_p| |\theta_f'(\omega_p)| \leq \frac{2|\omega_p|}{\pi} \int_0^\infty \left( A_f(\omega) - A_f(\omega_p) \right) \frac{1}{\omega^2 - \omega_p^2} \, d\omega.
$$

Thus, (56) holds. Moreover, when $\omega_p = 0$, by Lemma 3 we have $\theta'_f(\omega_p) = \frac{2}{\pi} \int_0^\infty A_f(\omega)/\omega^2 \, d\omega$. Since $A_f(\omega) \leq 0$, we conclude that $\theta'_f(\omega_p) \leq 0$.

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Shinji Hara (Fellow, IEEE) received the B.S., M.S., and Ph.D. degrees in engineering from the Tokyo Institute of Technology (TITech), Tokyo, Japan, in 1974, 1976, and 1981, respectively. In 1984, he joined TITech as an Associate Professor and was a Full Professor for ten years. From 2002 to 2017, he was a Full Professor with the Department of Information Physics and Computing with the University of Tokyo (U Tokyo), Tokyo. He is Professor Emeritus of TITech. His current research interests include glocal control and system biology.

Dr. Hara was the recipient of many awards in control, including the George S. Axelby Outstanding Paper Award from the IEEE Control System Society (CSS) in 2006. He was the President of SICE, Japan, in 2009, a Vice President of the IEEE CSS, from 2009 to 2010, and an IFAC Council Member, from 2011 to 2017. He is a Fellow of IFAC and SICE.

Chung-Yao Kao (Member, IEEE) received the Sc.D. degree in mechanical engineering from the Massachusetts Institute of Technology, Cambridge, USA, in 2002. From 2002 to 2004, he was Postdoctoral Researcher with the Department of Automatic Control, Lund University, Lund, Sweden, the Mittag-Leffler Institute, Stockholm, Sweden, and the Division of Optimization and Systems Theory, Royal Institute of Technology, Stockholm, Sweden. From 2004 to 2009, he was a Senior Lecturer with the Department of Electrical and Electronic Engineering, University of Melbourne, Melbourne, Australia. In 2009, he joined the Department of Electrical Engineering, National Sun Yat-Sen University, Kaohsiung, Taiwan, where he is currently a Professor. His research interests include robust control, systems theory, and optimization.

Sei Zhen Khong received the bachelor of electrical engineering degree (with first class honours) and the Ph.D. degree in electrical engineering from the University of Melbourne, Melbourne, Australia, in 2008 and 2012, respectively. He was a Researcher with the Department of Electrical and Electronic Engineering, the University of Melbourne, the Department of Automatic Control, Lund University, Lund, Sweden, the Institute for Mathematics and its Applications, the University of Minnesota, Twin Cities, MN, USA, and with the Department of Electrical and Electronic Engineering, the University of Hong Kong, Hong Kong, China. His research interests include network control, robust control, systems theory, and extremum seeking control.

Tetsuya Iwasaki (Fellow, IEEE) received the B.S. and M.S. degrees in electrical engineering from the Tokyo Institute of Technology, Tokyo, Japan, in 1987 and 1990, and the Ph.D. degree in aeronautics and astronautics from Purdue University, West Lafayette, IN, USA, in 1993. He held faculty positions with Tokyo Tech and University of Virginia before joining the University of California at Los Angeles, CA, USA. His research interests include dynamics and control of neuromechanics, global pattern formation via local interactions, and robust/optimal control theories. Dr. Iwasaki was the recipient of several awards from NSF, SICE, IEEE, and ASME. He was a Senior/Associate Editor of several control journals.

Yutaka Hori (Member, IEEE) received the B.S. degree in engineering, and the M.S. and Ph.D. degrees in information science and technology from the University of Tokyo, Tokyo, Japan, in 2008, 2010, and 2013, respectively. From 2013 to 2016, he was a Postdoc with the California Institute of Technology, Pasadena, CA, USA. In 2016, he joined Keio University, Tokyo, Japan, where he is currently an Associate Professor. His research interests include feedback control theory and its applications to synthetic biomolecular systems. Dr. Hori is a Member of SICE and ISCIE.