Higher order nonlinear chirp scaling algorithm for medium Earth orbit synthetic aperture radar

Pengbo Wang
Wei Liu
Jie Chen
Wei Yang
Yu Han
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Pengbo Wang,a,b Wei Liu,b Jie Chen,a,* Wei Yang,a and Yu Han a
aBeihang University, School of Electronic and Information Engineering, Beijing 100191, China
bUniversity of Sheffield, Department of Electronic and Electrical Engineering, Sheffield S1 3JD, United Kingdom

Abstract. Due to the larger orbital arc and longer synthetic aperture time in medium Earth orbit (MEO) synthetic aperture radar (SAR), it is difficult for conventional SAR imaging algorithms to achieve a good imaging result. An improved higher order nonlinear chirp scaling (NLCS) algorithm is presented for MEO SAR imaging. First, the point target spectrum of the modified equivalent squint range model-based signal is derived, where a concise expression is obtained by the method of series reversion. Second, the well-known NLCS algorithm is modified according to the new spectrum and an improved algorithm is developed. The range dependence of the two-dimensional point target reference spectrum is removed by improved CS processing, and accurate focusing is realized through range-matched filter and range-dependent azimuth-matched filter. Simulations are performed to validate the presented algorithm. © The Authors. Published by SPIE under a Creative Commons Attribution 3.0 Unported License. Distribution or reproduction of this work in whole or in part requires full attribution of the original publication, including its DOI. [DOI: 10.1117/1.JRS.9.096084]

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1 Introduction

Synthetic aperture radar (SAR) is a well-established remote sensing technique, capable of acquiring images of Earth’s surface independent of weather conditions and sunlight illumination.1 Since SEASAT was launched in 1978,2 spaceborne SAR has received much attention for its capabilities of Earth observation and environment monitoring. So far, most existing spaceborne SAR systems operate at the low Earth orbit (LEO) near or below 800 km.3 Because of their orbit height, the limitations of LEO-SAR are obvious, such as a long revisit period and narrow mapping swath. Compared with LEO SAR, the medium Earth orbit (MEO) SAR has better accessibility and greater coverage.4,5 However, along with the ascension of the orbit, the relative Satellite-Earth geometry of the MEO SAR will significantly deviate from a straight line, which poses many challenges for spaceborne SAR signal processing, particularly the imaging part.

An accurate range model and efficient imaging algorithm are the basis of MEO SAR signal processing. The most well-known range model in spaceborne SAR is the hyperbolic range equation model (HREM),6,7 which is derived from the straight track and is adapted to the curved orbit of spaceborne SAR by equivalent velocity and squint angle. However, for MEO SAR systems, the much longer integration time will introduce significant phase errors in signal processing based on old range models. Eldhuset8,9 proposed a fourth-order Doppler range model (DRM4) to describe the range history of high-resolution spaceborne SAR, where the third- and fourth-order phase errors can be fully compensated and a better imaging result can be obtained. However, the model does not consider the effect of higher order phase errors, which limits its application in MEO SAR. An advanced HREM for MEO SAR was proposed by Huang et al.10 where an additional linear term is introduced into the conventional HREM so

*Address all correspondence to: Jie Chen, E-mail: chenjie@buaa.edu.cn

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that it can handle the focusing issue of an azimuth resolution around 3 m at altitudes ranging from 1000 to 10,000 km. However, for higher altitudes, its performance degrades dramatically. The method of series reversion is another range model for spaceborne SAR imaging,\(^{11}\) where the range equation is expressed by a series expansion, and its accuracy is dependent on the number of terms used. To meet the requirements of MEO SAR imaging, more than four terms are needed in the expansion, which results in a high-complexity system. In this paper, a modified equivalent squint range model (MESRM), which was employed in our work in Ref. 12, is used as the range model for MEO SAR.

The chirp scaling (CS) algorithm is a common approach adopted for the processing of spaceborne SAR data due to its good phase preservation and high efficiency properties.\(^{13}\) However, the traditional CS algorithm was derived based on HREM and cannot be directly applied to our MESRM. In this work, we derive the point target spectrum (PTS) of the MESRM-based signal, and develop an improved higher order nonlinear chirp scaling (NLCS) algorithm for MEO SAR imaging where the improved CS processing is applied to remove the range dependence of a two-dimensional (2-D) point target reference spectrum (PTRS), and the higher order phase compensation, range-matched filter, and range-dependent azimuth filter are used to realize accurate focusing. Extensive simulations are performed to show the significantly improved imaging result.

This paper is organized as follows: with a brief description of the MESRM, the PTS based on MESRM is derived in Sec. 2. The corresponding improved algorithm for MEO SAR is developed in Sec. 3. Simulation results are provided in Sec. 4, and conclusions are drawn in Sec. 5.

## 2 Signal Model for Medium Earth Orbit Synthetic Aperture Radar

### 2.1 Range Model

The spaceborne SAR geometry in Earth-centered rotating coordinates is illustrated in Fig. 1, where the actual path is represented by the black solid line, and the paths based on HREM and MESRM are denoted by the blue dotted line and red dashed lines, respectively. For a short integration time, the straight path approximation is sufficient in the LEO cases. However, for the MEO SAR, the straight path approximation cannot properly fit the actual path and another degree of freedom should be used to make the range model more accurate. To improve the precision of the range model, an additional cubic component and quartic component are introduced in the range equation,\(^{12}\) as shown below:

![Fig. 1 Geometry of a typical spaceborne synthetic aperture radar (SAR).](image)
be described as

\[ R(t, r_0) = \sqrt{r_0^2 + v_0^2 t^2 - 2r_0 v_0 t \cos \varphi_0 + \Delta \alpha_3 t^3 + \Delta \alpha_4 t^4}, \]

where \( t \) is the azimuth time, \( r_0 \) is the slant range at Doppler center time, \( v_0 \) is the equivalent velocity between the scatterer and the SAR, \( \varphi_0 \) is the equivalent squint angle, \( \lambda \) is the signal wavelength, and \( f_{d0}, f_{t0}, f_{r0}, \text{ and } f_{a0} \) denote the Doppler centroid frequency, the azimuth FM rate, the rate of the azimuth FM rate and the second-order derivative of the azimuth FM rate, respectively, given by

\[ f_{a0} = -2\frac{2(V_{sat} - V_{tar}) \cdot (R_{sat} - R_{tar})}{\lambda r_0}, \]

\[ f_{t0} = -2\frac{2(A_{sat} - A_{tar}) \cdot (R_{sat} - R_{tar}) - 2(V_{sat} - V_{tar}) \cdot (V_{sat} - V_{tar})}{\lambda r_0} + \frac{\lambda f_{a0}^2}{2r_0}, \]

\[ f_{r0} = -2\frac{2(A'_{sat} - A'_{tar})(R_{sat} - R_{tar}) - 6(A_{sat} - A_{tar})(V_{sat} - V_{tar})}{\lambda r_0} + \frac{3\lambda f_{a0} f_{t0}}{2r_0}, \]

\[ f_{a4} = -2\frac{8(A''_{sat} - A''_{tar})(V_{sat} - V_{tar}) - 6(A_{sat} - A_{tar})(A_{sat} - A_{tar})}{\lambda r_0} + \frac{24\lambda f_{a0} f_{r0}^2}{2r_0} + \frac{3\lambda f_{a0} f_{t0} f_{r0}}{r_0}, \]

where \( R, V, A, A' \) and \( A'' \) denote the position vector, velocity vector, acceleration vector, and the rate of the acceleration vector and its second-order derivative, respectively. The subscript sat represents the satellite, and tar represents the ground target. Compared with the traditional range model, the MESRM not only perfectly compensates the actual range history up to the quartic term, but also partially compensates the higher order terms, which makes MESRM more suitable for MEO SAR.

### 2.2 Signal Model

Based on the MESRM, after demodulation to baseband, the received signal for a point target can be described as

\[ S(t, \tau) = \sigma_0 \cdot \omega_\tau(t-t_0) \cdot \omega_\varphi \left[ \tau - \frac{2R(t)}{c} \right] \cdot \exp \left\{ -j4\pi \frac{R(t)}{\lambda} \right\} \cdot \exp \left\{ j\pi K_r \left[ \tau - \frac{2R(t)}{c} \right]^2 \right\}, \]

where \( \sigma_0 \) represents the scattering coefficient, \( \omega_\varphi(\cdot) \) and \( \omega_\tau(\cdot) \) denote antenna pattern functions in the range and azimuth directions, respectively, \( c \) is the speed of light, \( K_r \) is the range chirp rate, \( \tau \) is the fast time, and \( t_0 \) is the Doppler center time of point target.

In order to obtain the 2-D PTS of the above echo expression, the principle of stationary phase and Fourier transformation (FT) is applied. The 2-D PTS of the echo signal can be obtained as
\[ S(f_r, f_s) = \sigma_0 \cdot \omega_0 \cdot [s(f_r, f_s)] \cdot \omega_r(f_r) \cdot \exp\left\{-j\frac{\pi f_c^2}{K_r}\right\} \]
\[ \cdot \exp\left\{-j4\pi \left(\frac{1}{\lambda} + \frac{f_c}{c}\right) R[t_a(f_r, f_s)]\right\} \cdot \exp\left\{-j2\pi f_s t_a(f_r, f_s)\right\}, \]

where \( f_c \) is the range frequency, \( f_s \) is the azimuth frequency, and \( t_a(\cdot) \) is the stationary point obtained by solving the following equation:
\[ 2\left(\frac{1}{\lambda} + \frac{f_c}{c}\right) \frac{\partial R[t_a(f_r, f_s)]}{\partial t} + f_a = 0. \]

Considering the complexity of the range model, it is difficult to find a closed-form solution for the stationary point. To facilitate the derivation of the following imaging algorithm, we expand the signal phase by a power series with respect to \( f_r \), as follows:
\[ S(f_r, f_s; r_0) = \sigma_0 \omega_0 \cdot [s(f_a, f_s)] \cdot \omega_r(f_r) \cdot \exp\{\Phi_{azi}(f_s; r_0)\} \cdot \exp\{\Phi_{RCM}(f_r, f_s; r_0)\} \]
\[ \cdot \exp\{\Phi_{tg2}(f_r, f_s; r_0)\} \cdot \exp\{\Phi_{HOP}(f_r, f_s; r_0)\}, \]

where
\[ \Phi_{azi}(f_s; r_0) = -j\frac{4\pi}{\lambda} \left[r_0 - \frac{\lambda^2(f_a - f_d)^2}{8} + \frac{\lambda^3(f_a - f_d)^3}{24} - \frac{\lambda^4(f_a - f_d)^4}{64} \right], \]

\[ \Phi_{RCM}(f_r, f_s; r_0) = -j\frac{4\pi}{c} \left[r_0 + \frac{\lambda^2(f_a + f_d)(f_a - f_d)}{8} \right. \]
\[ \left. - \frac{\lambda^3(2f_a + f_d)(f_a - f_d)^2}{24} + \frac{\lambda^4(3f_a + f_d)(f_a - f_d)^3}{64} \right] \cdot f_r, \]

\[ \Phi_{tg2}(f_r, f_s; r_0) = -j\frac{\pi f_c^2}{K_r} + j\pi \left[\frac{\lambda^2 f_d^2}{2f_c^2} \cdot f_r - \frac{\lambda^2 f_d^2}{2f_c^2} \cdot f_r + \frac{3\lambda^3 f_d^2}{8f_c^2} \right] \cdot f_r, \]

\[ \Phi_{HOP}(f_r, f_s; r_0) = -j4\pi \left(\frac{1}{\lambda} + \frac{f_c}{c}\right) R[t_a(f_s, f_s; r_0)] - j2\pi f_s t_a(f_s, f_s; r_0) \]
\[ - \Phi_{azi}(f_s; r_0) - \Phi_{RCM}(f_r, f_s; r_0) - \Phi_{tg2}(f_r, f_s; r_0) - j\frac{\pi f_c^2}{K_r}, \]

where \( f_c \) is the carrier frequency and \( \alpha, \beta, \gamma \) are the Doppler parameters of the echo signal, given by
\[ \alpha = \frac{r_0}{v_{t_0} \sin \phi_{t_0}^0}, \]

\[ \beta = -\frac{3\Delta \alpha_0 r_0^3}{2v_{t_0} \sin \phi_{t_0}^0} - \frac{3r_0 \cos \phi_{t_0}^0}{2v_{t_0} \sin \phi_{t_0}^0}, \]

\[ \gamma = -\frac{2\Delta \alpha_0 r_0^3}{v_{t_0} \sin \phi_{t_0}^0} + \frac{9\Delta \alpha_0 r_0^3}{2v_{t_0} \sin \phi_{t_0}^0} + \frac{7\Delta \alpha_0 r_0^3}{2v_{t_0} \sin \phi_{t_0}^0} + \frac{9r_0 \cos \phi_{t_0}^0}{2v_{t_0} \sin \phi_{t_0}^0} + \frac{r_0(1 - 5 \cos \phi_{t_0}^0)}{2v_{t_0} \sin \phi_{t_0}^0}. \]

From Eqs. (15) to (17), it can be seen that the Doppler parameters \( \alpha, \beta, \gamma \) vary with range \( r_0 \), which increases the difficulty for the following imaging process. Figure 2 shows the curve of the Doppler parameters with respect to slant range displacement. There is a nearly linear
relationship between the Doppler parameters and the range displacement. To describe the range
dependence of the Doppler parameters, a linear hypothesis is used to deduce the following im-
ing algorithm, which is given by

\[
\begin{align*}
\alpha &= \alpha_1 + \alpha_2 (r_0 - r_{\text{ref}}) \\
\beta &= \beta_1 + \beta_2 (r_0 - r_{\text{ref}}) \\
\gamma &= \gamma_1 + \gamma_2 (r_0 - r_{\text{ref}})
\end{align*}
\]

Substituting Eqs. (18) into (10), the PTS based on the MESRM can be obtained, and the
corresponding improved imaging algorithm is presented in the following section.

3 Higher Order Chirp Scaling Algorithm

Based on the proposed signal model in Sec. 2, an improved imaging algorithm is presented here:
higher order cross-coupling is removed by higher order phase compensation, the accurate range
cell migration correction (RCMC) and secondary range compressed (SRC) are accomplished by
the improved CS processing, and accurate azimuth focusing is achieved through the range-de-
dendent azimuth-matched filtering. The block diagram of our proposed algorithm is shown in
Fig. 3. In the following, details of the basic operations are provided according to the signal flow
in the diagram.

It starts with higher order phase compensation and cubic phase filtering in the 2-D frequency
domain, where cubic phase filtering is used to provide the most accurate accommodation of
range dependence of SRC, and the higher order cross-coupling is removed by the higher
order phase compensation. The higher order phase function and cubic phase function are
given by

\[
H_1(f_a; f_\tau; r_0) = \exp\{-\Phi_{\text{HOP}}(f_\tau, f_a; r_0)\},
\]

\[
H_2(f_a; f_\tau; r_0) = \exp\left\{\frac{2\pi}{3} Y(f_a) f_\tau^2\right\},
\]

where \( Y(f_a) \) is the azimuth-frequency varying cubic phase filter coefficient, given by

\[
Y(f_a) = \frac{4\lambda f_a^2 \alpha_2 - 4\lambda^2 f_a^2 (f_a - f_d) \beta_2 + 3\lambda^3 f_a^2 (f_a - f_d)^2 \gamma_2}{8 f_a^2 K_m(f_a; r_0) |\tau_2^2(f_a) + 2\tau_2(f_a)|}.
\]

After higher order phase compensation and cubic phase filtering, the signal is transformed
into the range-Doppler domain by range inverse FFT (IFFT). Considering that the cubic phase
term is small enough, the range-Doppler domain representation of the filtered signal can then be
written as

\[
S(\tau, f_a; r_0) = \sigma_0 \alpha_1(\tau, f_a) \cdot \alpha_1(\tau) \cdot \exp\left\{j \pi K_m(f_a; r_0) |\tau - \tau_0(f_a; r_0)|^2\right\}
\]

\[
\cdot \exp\left\{\frac{2\pi}{3} Y(f_a) K_m(f_a; r_0)^3 |\tau - \tau_0(f_a; r_0)|^3\right\} \cdot \exp\{\Phi_{\text{azi}}(f_a; r_0)\}.
\]
where

\[
\frac{1}{K_m(f_a; r_0)} = \frac{1}{K_r} - \left[ \frac{\lambda_1 f_0^2}{2f_c} \alpha_1 - \frac{\lambda_2 f_0^2 f_a - f_d}{2f_c^2} \beta_1 + \frac{3\lambda_3 f_0^2 (f_a - f_d)^2}{8f_c^2} \gamma_1 \right] \\
- \left[ \frac{\lambda_1 f_0^2}{2f_c^2} \alpha_2 - \frac{\lambda_2 f_0^2 f_a - f_d}{2f_c^2} \beta_2 + \frac{3\lambda_3 f_0^2 (f_a - f_d)^2}{8f_c^2} \gamma_2 \right] (r_0 - r_{ref}),
\]

\( \tau_d(f_a; r_0) = \frac{2r_0}{c} + \tau_1(f_a) + \tau_2(f_a)(r_0 - r_{ref}), \)

\( \tau_1(f_a) = \frac{\lambda_2 (f_a^2 - f_d^2)}{4c} \alpha_1 - \frac{\lambda_3 (2f_a + f_d)(f_a - f_d)^2}{12c} \beta_1 + \frac{\lambda_4 (3f_a + f_d)(f_a - f_d)^3}{32c} \gamma_1, \)

\( \tau_2(f_a) = \frac{\lambda_2 (f_a^2 - f_d^2)}{4c} \alpha_2 - \frac{\lambda_3 (2f_a + f_d)(f_a - f_d)^2}{12c} \beta_2 + \frac{\lambda_4 (3f_a + f_d)(f_a - f_d)^3}{32c} \gamma_2. \)

To remove the range dependence of SRC and RCM, NLCS processing is performed, where the NLCS function \( H_3(\tau, f_a), \) centered at the reference range \( \tau_d(f_a; r_{ref}), \) is given by

\( H_3(\tau, f_a) = \frac{1}{K_m(f_a; r_0)} - \left[ \frac{\lambda_1 f_0^2}{2f_c} \alpha_1 - \frac{\lambda_2 f_0^2 f_a - f_d}{2f_c^2} \beta_1 + \frac{3\lambda_3 f_0^2 (f_a - f_d)^2}{8f_c^2} \gamma_1 \right] \\
- \left[ \frac{\lambda_1 f_0^2}{2f_c^2} \alpha_2 - \frac{\lambda_2 f_0^2 f_a - f_d}{2f_c^2} \beta_2 + \frac{3\lambda_3 f_0^2 (f_a - f_d)^2}{8f_c^2} \gamma_2 \right] (\tau - \tau_d(f_a; r_{ref})). \)
\[ H_3(\tau, f_a) = \exp\left\{ -\frac{2\pi}{3} q_3(f_a) [\tau - \tau_d(f_a; r_{\text{ref}})]^3 - j\pi q_2(f_a) [\tau - \tau_d(f_a; r_{\text{ref}})]^2 \right\} \]  

(27)

where \( q_3(f_a) \) and \( q_2(f_a) \) denote the quadratic and cubic coefficients

\[ q_3(f_a) = \frac{c^2}{4} Y(f_a) K_m(f_a; r_{\text{ref}})^3 \tau_2(f_a)^2. \]  

(28)

\[ q_2(f_a) = -K_m(f_a; r_{\text{ref}}) \tau_2(f_a) \frac{c}{2}. \]  

(29)

After NLCS processing, the signal can be expressed as

\[ S(\tau, f_a; r_0) = \sigma_0 a_t[\tau(f_a), f_a] \cdot \sigma_i(\tau) \cdot \exp\{\Phi_{\text{azi}}(f_a; r_0)\} \exp\{\Phi_0(f_a; r_0)\} \]

\[ \cdot \exp\left\{ j\pi K_m(f_a; r_{\text{ref}}) \left[ 1 + \tau_2(f_a) \frac{c}{2} \right] \left[ \tau - \frac{2r_0}{c} - \tau_1(f_a) \right]^2 \right\} \]

\[ \cdot \exp\left\{ -j\frac{2\pi}{3} Y(f_a) K_m(f_a; r_{\text{ref}})^3 \left[ 1 - \tau_2(f_a)^2 \right] \left[ \tau - \frac{2r_0}{c} - \tau_1(f_a)^3 \right]^3 \right\}. \]  

(30)

where

\[ \Phi_0(f_a; r_0) = j\pi K_m(f_a; r_0) \tau_2(f_a)^2 (r_0 - r_{\text{ref}})^2 - j\frac{2\pi q_2}{c} (r_0 - r_{\text{ref}})^2 \]

\[ - j\frac{2\pi}{3} Y(f_a) K_m(f_a; r_0)^3 \tau_2(f_a)^3 (r_0 - r_{\text{ref}})^3 + j\frac{16\pi q_3}{3c^3} (r_0 - r_{\text{ref}})^3. \]  

(31)

From Eq. (30), it can be seen that the RCMC and SRC are independent of range \( r_0 \), and the bulk RCMC and SRC can be performed accurately and efficiently across the range swath. Accordingly, the range processing filter \( H_4(f_r, f_a) \) is given by

\[ H_4(f_r, f_a) = \exp\{j2\pi f_r \tau_1(f_a)\} \cdot \exp\left\{ j\pi \frac{f_r^2}{K_m(f_a; r_{\text{ref}}) \left[ 1 + \tau_2(f_a) \frac{c}{2} \right]} \right\} \]

\[ \cdot \exp\left\{ -j\pi \frac{2Y(f_a) \left[ 1 - \tau_2(f_a)^2 \right] f_r^3}{3 \left[ 1 + \tau_2(f_a) \frac{c}{2} \right]^3} \right\}. \]  

(32)

After the range IFFT takes the data back to the range-Doppler domain, range-dependent azimuth-matched filtering and residual phase compensation can be performed by the azimuth processing filter \( H_5(f_a) \)

\[ H_5(f_a; r_0) = \exp\{ -\Phi_{\text{azi}}(f_a; r_0)\} \cdot \exp\{ -\Phi_0(f_a; r_0)\}. \]  

(33)

Finally, a well-focused target is generated by the azimuth IFFT.

### 4 Simulations and Analyses

Now, simulations are performed to first validate the MESRM for MEO SAR. Then, the accuracy of the derived 2-D spectrum is verified with a different azimuth resolution. Finally, the performance of our proposed imaging algorithm is demonstrated. The simulation parameters are listed in Table 1.
Simulation for Modified Equivalent Squint Range Model

The capability of a given range model is mainly determined by the azimuth phase error. To show the accuracy of the MESRM, the azimuth phase errors caused by range deviation as a function of orbit altitude are provided in Fig. 4, where the azimuth resolution is set to be 1.5 m, and the other parameters are listed in Table 1. It can be clearly seen that the MESRM is more accurate than the ESRM, AESRM, and DRM4. Under the azimuth phase criterion of $0.25\pi$, MESRM performs very well up to 12,000 km, whereas the performance of the AESRM degrades dramatically above 1700 km. Figure 5 illustrates the phase errors caused by range deviation as a function of the synthetic aperture time. It is shown that, under the azimuth phase error criterion of $0.25\pi$, the maximal synthetic aperture time for MESRM is up to 300 s. As a result, an azimuth resolution higher than 1.5 m can be achieved.

Simulation for Two-Dimensional Spectrum

The 2-D PTS is the basis of an imaging algorithm. To verify the accuracy of the 2-D spectrum, we compress the echo signal with the 2-D spectrum based on MESRM, AESRM, and DRM4.

Table 1 Simulation parameters for modified equivalent squint range model (MEO SAR).

| Parameter                | Value               |
|--------------------------|---------------------|
| Semi-major               | 16,378 km           |
| Eccentricity             | 0.00                |
| Inclination              | 90 deg              |
| Argument of perigee      | 90 deg              |
| Wavelength               | 0.24 m              |
| Bandwidth                | 150.0 MHz           |
| Look angle               | 15.0 deg            |
| Azimuth resolution       | 3.0 m               |
| Antenna length           | 25.8 m              |
| Antenna width            | 11.8 m              |
| Doppler centroid         | $-2.09 \text{ Hz}$  |
| Azimuth FM rate          | $5.30 \text{ Hz/s}$ |
| $f_{r3}$                 | $-0.44 \text{ mHz/s}^2$ |
| $f_{r4}$                 | $-1.33 \text{ mHz/s}^3$ |

Fig. 4 Phase error caused by range deviation as a function of orbit altitude.
The impulse response widths (IRWs) (normalized to the theoretical value) and the peak sidelobe ratio (PSLR) with respect to azimuth resolution are plotted in Figs. 6 and 7, respectively. It can be seen that the 2-D spectrum can maintain sufficient accuracy even if the azimuth resolution is up to 1.5 m, where the deterioration of IRWs is less than 1% and the degradation of PSLR is less than 0.4 dB, which can meet the requirements of MEO SAR.

4.3 Simulation for Algorithm

To demonstrate the performance of the proposed imaging algorithm, raw data are first generated in our simulation for point targets using the parameters given in Table 1, with the scene shown in

![Fig. 5 Phase error caused by range deviation as a function of the (SAR).](image)

![Fig. 6 Impulse response width (IRW) as a function of azimuth resolution.](image)

![Fig. 7 Peak sidelobe ratio (PSLR) as a function of azimuth resolution.](image)
The distances of different targets along the range and azimuth are 40.0 and 0.6 km, respectively. Moreover, rectangular weighting is used for both azimuth and range processing. The focused result of the NLCS algorithm is shown in Fig. 9 for comparison, where the HREM is used and the corresponding parameters are calculated for each range bin. It can be seen that the focused results suffer from severe degradation, and significant azimuth mainlobe broadening and sidelobe rising are observed for all targets. Figure 10 shows the focused result based on our proposed algorithm. The interpolated contours of PT1, PT5, and PT9 are presented in Fig. 11 to evaluate the image quality. Compared to the NLCS algorithm result, the focusing performance has been significantly improved. To quantify the focusing performance, the point target analysis results are listed in Table 2, where the subscript $m$ represents the measured value, and $c$ represents the calculated value. The ideal PSLR and the integrated sidelobe ratio (ISLR) are 13.26 and 9.68 dB, respectively, using the rectangular window.

![Fig. 8 Targets distribution in the simulated scene.](image)

![Fig. 9 Focused result by the NLCS algorithm.](image)

![Fig. 10 Focused result by the proposed algorithm.](image)
According to Table 2, it can be seen that the deterioration of IRW in the range direction is less than 1% and that in the azimuth direction is less than 1.5%. The PSLRs and ISLRs have less than 5% degradation in both the azimuth and range directions. All these indicate that the corresponding focusing algorithm can effectively meet the imaging requirement of the MEO SAR.

Location is another index with which to evaluate the performance of imaging algorithms. Table 3 shows position deviations of all targets after being compressed, where the

| Point targets | Position in imaging scene (m) | Position in focused scene (m) | Position deviation (m) |
|---------------|------------------------------|------------------------------|------------------------|
| PT1           | (11031287.70, −660.32)       | (11031287.52, −660.55)       | (−0.18, −0.23)         |
| PT2           | (11031214.66, 1.40)          | (11031214.48, 1.58)          | (−0.18, 0.18)          |
| PT3           | (11031141.65, 657.55)        | (11031141.36, 657.31)        | (−0.19, −0.24)         |
| PT4           | (11058435.71, −662.63)       | (11058435.73, −662.87)       | (−0.02, −0.25)         |
| PT5           | (11058359.89, 0.00)          | (11058359.89, −0.25)         | (0.00, −0.25)          |
| PT6           | (11058284.10, 662.63)        | (11058284.05, 662.37)        | (−0.05, −0.26)         |
| PT7           | (11085986.48, −660.73)       | (11085986.33, −660.88)       | (−0.15, −0.15)         |
| PT8           | (11085907.85, 5.70)          | (11085907.67, 5.48)          | (−0.18, −0.22)         |
| PT9           | (11085929.27, 672.09)        | (11085829.02, 671.91)        | (−0.25, −0.18)         |
slant-range imaging plane is taken as the reference. We can see that position deviation in both the range and azimuth directions is less than 0.3 m, showing a high location accuracy for our proposed algorithm.

5 Conclusion

For MEO spaceborne SAR, an improved higher order NLCS algorithm based on MESRM has been proposed in this paper, which takes into account the curved orbit and the range dependence of the PTS. Based on the MESRM, the corresponding signal model as well as the PTS have been derived. A modified higher order imaging algorithm has also been developed, where higher order phase compensation is introduced to remove higher order cross-coupling, and accurate focusing is achieved by the improved NLCS algorithm. Simulation results have been provided to verify the effectiveness of the proposed model and the corresponding imaging algorithm.

Appendix: Derivation of Two-Dimensional Point Target Spectrum

To derive the 2-D PTS of the echo signal, we first expand the range model by power series with respect to \( t \)

\[
R(t, r_0) = r_0 - v_0 \cos \varphi_0 t + \frac{v_0^2 \sin \varphi_0^2}{2r_0} t^2 + \frac{\Delta \varphi^2 + \frac{v_0^3 \cos \varphi_0 \sin \varphi_0^2}{2r_0}}{2r_0^2} t^3 + \ldots
\]

Applying the series reversion in Eq. (9)\(^5\) yields the following 2-D spectrum

\[
S(f_r, f_a; r_0) = \sigma_0 \omega_a(f_a) \cdot \omega_r(f_r) \cdot \exp\{\Phi_{\text{PTRS}}(f_a; r_0)\} \cdot \exp\{\Phi_{\text{HOP}}(f_r, f_a; r_0)\},
\]

where

\[
\Phi_{\text{PTRS}}(f_r, f_a; r_0) = -\frac{4\pi(f_r + f_a)}{c} \left( r_0 - \frac{M^2 r_0}{2V_0^2 \sin \varphi_0^2} + \frac{M^4 \Delta \varphi^2 r_0^2}{2V_0^2 \sin \varphi_0^2} + \frac{M^4 \varphi_0}{2V_0^2 \sin \varphi_0^2} \right)
\]

\[
- \frac{\pi(f_r + f_a)M^4}{c} \left( \frac{2\Delta \varphi^4 r_0^3}{V_0^2 \sin \varphi_0^2} + \frac{9\Delta \varphi^4 r_0^3}{2V_0^2 \sin \varphi_0^2} + \frac{9\Delta \varphi^4 r_0^3 \cos \varphi_0}{V_0^4 \sin \varphi_0^2} \right)
\]

\[
- \frac{\pi(f_r + f_a)M^4}{c} \left( \frac{7r_0 \cos \varphi_0^2}{2V_0^4 \sin \varphi_0^2} \cos \varphi_0 + \frac{r_0 (1 - 5 \cos \varphi_0^2)}{2V_0^4 \sin \varphi_0^2} \right).
\]

\[
M = -\frac{\pi c}{2(f_r + f_a)} + \frac{4f_a}{c}.
\]

Next, we expand the signal phase by power series with respect to \( f_r \), as follows:

\[
\Phi_{\text{PTRS}}(f_r, f_a; r_0) = \Phi_{\text{are}}(f_a; r_0) + \Phi_{\text{RCM}}(f_r, f_a; r_0) + \Phi_{\text{eg2}}(f_r, f_a; r_0) + \Phi_{\text{HOP}}'(f_r, f_a; r_0).
\]

Finally, we merge \( \Phi_{\text{HOP}}' \) with \( \Phi_{\text{HOP}}'' \), and the 2-D PTS in Eq. (10) can be obtained.

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Pengbo Wang received his PhD degree in information and communication engineering from Beihang University, Beijing, China, in 2007. Since July 2010, he has been with the school of Electronics and Information Engineering, Beihang University (BUAA), as a lecturer. His current research interests include high-resolution spaceborne synthetic aperture radar (SAR) image formation, novel techniques for spaceborne SAR systems, and multimodal remote sensing data fusion.

Wei Liu received his PhD degree in 2003 from the School of Electronics and Computer Science, University of Southampton, United Kingdom. Since September 2005, he has been with the Communications Research Group, Department of Electronic and Electrical Engineering, University of Sheffield, United Kingdom, as a lecturer. His research interests include sensor array signal processing, blind signal processing, multirate signal processing and their various applications in wireless communications, sonar, radar, satellite navigation, speech enhancement, and biomedical engineering.

Jie Chen received his BS and PhD degrees from Beihang University, China, in 1996 and 2002, respectively. He is a professor with the School of Electronics and Information Engineering, Beihang University (BUAA) from 2004. His current research interests include remote sensing information acquisition and signal processing, topside ionosphere exploration based on spaceborne HF-SAR, high-resolution spaceborne SAR image formation, and modeling and simulation for spaceborne SAR systems.

Wei Yang received his MS and PhD degrees from Beihang University, China, in 2008 and 2011, respectively. He has been a lecturer with the School of Electronics and Information Engineering, Beihang University, since 2013. His current research interests include high-resolution spaceborne SAR image formation and modeling and simulation for spaceborne SAR systems.

Yu Han received his BS degree from Beihang University in 2012. Currently, he is working toward his MS degree at Beihang University. His research interest includes high-resolution spaceborne SAR image formation.