System-Level Analysis of Joint Sensing and Communication based on 5G New Radio

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Abstract—This work investigates a multibeam system for joint sensing and communication (JSC) based on multiple-input multiple-output (MIMO) 5G new radio (NR) waveforms. In particular, we consider a base station (BS) acting as a monostatic sensor that estimates the range, speed, and direction of arrival (DoA) of multiple targets via beam scanning using a fraction of the transmitted power. The target position is then obtained via range and DoA estimation. We derive the sensing performance in terms of probability of detection and root mean squared error (RMSE) of position and velocity estimation of a target under line-of-sight (LOS) conditions. Furthermore, we evaluate the system performance when multiple targets are present, using the optimal sub-pattern assignment (OSPA) metric. Finally, we provide an in-depth investigation of the dominant factors that affect performance, including the fraction of power reserved for sensing.

Index Terms—Joint sensing and communication, 5G New Radio, multiple antennas, beamforming, multiple target detection, root mean squared error, localization error, optimal sub-pattern assignment metric.

I. INTRODUCTION

The widespread diffusion of increasingly broadband mobile radio networks and the conquest of mmWave by 5G communication systems has exacerbated the spectrum congestion. On the other hand, sensing capabilities via radio frequency (RF) signals are gaining increasing interest for several applications, such as autonomous driving, assisted living, security, and human-machine interface [2]. In the framework of this trend, we are witnessing an increasing demand for systems exhibiting both sensing and communications capabilities, i.e., systems where radar and communication functionalities share the hardware platform, as well as the frequency band [3], [4]. This approach is also known as joint sensing and communication (JSC) and consists in exploiting the waveforms transmitted by a communication network to perform sensing functions. In this scenario, orthogonal frequency division multiplexing (OFDM) based signals are considered good candidates both for active and passive radar purposes. For example, in [5] and [6] OFDM-based communication systems such as long term evolution (LTE) and 5G new radio (NR) are suggested. In [7] the self-ambiguity function (SAF) and cross-ambiguity function (CAF) for the frequency division duplex (FDD) LTE downlink waveform are evaluated. Another possible solution, widely explored in literature, is represented by passive radars relying on signals of opportunity. In this case, the problem of the spectrum sharing is solved by removing the radar sources, i.e., by performing localization and tracking of targets without the need for radar signals emissions but only by exploiting illuminators of opportunity already present in the environment [8], [9]. However, the radar system does not have full knowledge about the transmitted signals and can only perform detection and estimation based on the power, angles, and Doppler information extracted from the received echo [10].

In [4] applications of JSC systems are discussed. According to [11], JSC can be studied focusing on both simple point-to-point communications such as vehicular networks [12]–[17] (thus finding great applications in autonomous driving) and complex mobile/ cellular networks [10], [18]–[20], which can potentially revolutionize the current communication-only mobile networks. JSC also has the potential of integrating radio sensing into large-scale mobile networks, generating the so-called perceptive mobile networks [10], [21]–[24]. Moreover, literature on mmWave JSC demonstrates its feasibility and potentials in indoor and vehicle networks [12], [15], [25]–[30]. In particular, in-depth signal processing aspects of mmWave-based JSC with an emphasis on waveform design are provided by [25]. At mmWave frequencies, multiple-input multiple-output (MIMO) systems enable very high capacity links and reduced latencies to the communication users through spatial multiplexing, while also providing augmented sensing capabilities due to accurate direction of arrival (DoA) estimation [31], [32].

Some research studies on JSC mainly focus on single beam approaches per phased array, having the sensing beam in the same direction of the communication beam [33]. To overcome this problem, recent studies have focused on using separate coexisting beams for communication and sensing due to the very different requirements of the two functionalities. For example, in [12], [34] a multibeam framework consisting of beamforming design and optimization are proposed to simultaneously allow a steady communication beam towards the user equipment (UE) and a sensing beam to scan the environment.

Most of the research efforts on JSC have so far been...
devoted to the design of signal processing techniques aimed at extracting features from the environment, such as the position and speed of a target (for example, a car or a human being) or at inferring the environment itself, such as the mapping or imaging of a room. However, to the authors’ knowledge, very few works have investigated the performance of a JSC system, especially from the sensing perspective, and provided results in terms of target parameters estimation accuracy with current technology. For this reason, this work aims to address the analysis of a multibeam system for JSC based on 5G NR to understand the key aspects and their role in governing performance. In particular, the main contributions are the following:

- We provide an analysis of the performance of a base station (BS) acting as a sensor in a monostatic configuration that estimates the range, speed, and DoA of multiple targets, through numerical simulations. In particular, we provide a detailed analysis of how the system performance is affected by the portion of the total radiated power used for sensing. Furthermore, we propose an algorithm to remove phantom targets that appear because of the sensing method, which relies on beam-scanning impaired by beam sidelobes.
- We analyze the root mean squared error (RMSE) of position estimation, obtained by target localization via range and DoA estimation, and the accuracy of radial speed estimation for the single-target scenario.
- We identify the main dominant factors affecting performance and compare two system setups operating at sub-6 GHz and mmWave frequencies.
- We use the optimal sub-pattern assignment (OSPA) metric to study the performance of the considered system for the multi-target scenario at mmWave frequencies in terms of localization and detection capabilities.

Throughout this paper, capital boldface letters denote matrices, lowercase bold letters indicate vectors, (·)\top, (·)\imath, and (·)\sp{c} stand for transpose, conjugate transpose, and conjugate of a vector/matrix respectively, \(\|\cdot\|_p\) is the \(p\)-norm operator, and \(\lceil\cdot\rceil\) is the ceiling function.

The paper is organized as follows. In Section II the system model and the proposed JSC scheme are described. Section III presents the adopted estimation techniques and the repeated targets pruning procedure. Section IV discusses the use of the OSPA metric to evaluate the performance of the multi-target system. In Section V an extensive performance analysis is presented. We then conclude this article with our remarks in Section VI.

II. SYSTEM MODEL

As depicted in Fig. 1 a multiple antennas OFDM system is considered. The JSC system consists of a transmitter (Tx) antenna array with \(N_T\) elements and of an receiver (Rx) antenna array with \(N_R\) elements, used for communication and sensing, respectively. For both Tx and Rx we assume a uniform linear array (ULA) with half-wavelength separation, i.e., \(d = \lambda/2\) with \(\lambda = c/f_c\), \(c\) the speed of light, and \(f_c\) the carrier frequency. The communication system transmits a 5G NR waveform with \(M\) OFDM symbols and \(K\) active subcarriers to a UE in the cell \([35]^{1}\). The equivalent low-pass (ELP) representation of the signal transmitted by the \(n\)th antenna can be written as

\[
s_n(t) = \sum_{m=0}^{M-1} \left( \sum_{k=0}^{K-1} x_{n,k}^{(m)} e^{j2\pi ft} \right) g(t - mT_s)
\]

(1)

where \(x_{n,k}^{(m)}\) is the modulation symbol, taken from a complex modulation alphabet, to be transmitted to the UE at the \(n\)th OFDM symbol and \(k\)th subcarrier, mapped through digital precoding at the \(n\)th transmitting antenna, \(g(t)\) is the employed pulse, \(\Delta f = 1/T_s\) is the subcarrier spacing, and \(T_s\) is the OFDM symbol duration including the cyclic prefix (CP).

A. Joint waveform

The vector \(x_k^{(m)} \in \mathbb{C}^{N_T \times 1}\) is defined as \(x_k^{(m)} = w_T x_k^{(m)}\), where \(w_T \in \mathbb{C}^{N_T \times 1}\) is the precoder vector used to map each modulation symbol, \(x_k^{(m)}\), to the transmitting antennas. In particular, we consider a multibeam system where the power of the OFDM signal to be transmitted is split between communication and sensing, namely, the total available power is in part exploited to sense the environment and in part directed to the UE \([12], [34]\). Therefore, the transmitting beamformer (BF) vector \(w_T\) can be written as \([12]\)

\[
w_T = \sqrt{\rho} w_{T,s} + \sqrt{1-\rho} w_{T,c}
\]

(2)

where \(\rho \in [0, 1]\) is the parameter used to control the fraction of the total power apportioned to the two directions, while \(w_{T,c}\) and \(w_{T,s}\) are the communication and the sensing BF vectors, respectively. The latter are defined as \([85]\)

\[
w_{T,c} = \frac{\sqrt{P_T G_T^c}}{N_T} a_T^c(\theta_{T,c})
\]

(3)

\[
w_{T,s} = \frac{\sqrt{P_T G_T^s}}{N_T} a_T^s(\theta_{T,s})
\]

(4)

where \(G_T^s\) is the transmit array gain along the beam steering direction (where such a gain is maximum), \(P_T G_T^c\) is the effective isotropic radiated power (EIRP), \(a_T(\theta_{T,c}) \in \mathbb{C}^{N_T \times 1}\) and \(a_T^s(\theta_{T,s}) \in \mathbb{C}^{N_T \times 1}\) are the steering vectors for communication and sensing, respectively. The spatial steering vector for a ULA at a given DoA/direction of departure (DoD) \(\theta_{T}\) is \([56] \text{ Chapter 9}, [35] \text{ Chapter 5}\)

\[
a(\theta_{T}) = \left[1, e^{j2\pi d \sin(\theta_{T})/\lambda}, \ldots, e^{j2\pi (N_T-1) \sin(\theta_{T})/\lambda}\right]^\top
\]

(5)

where \(N_T\) is the number of antenna elements. Since a half-wavelength separation is considered, the expression \([5]^{2}\) reduces to

\[
a(\theta_{T}) = \left[1, e^{j\pi \sin(\theta_{T})}, \ldots, e^{j\pi (N_T-1) \sin(\theta_{T})}\right]^\top.
\]

(6)

1Without loss of generality, we consider one user; however, during the scan period described in Section II-C the UE may change according to the multiple access rule established for communication.

2Without loss of generality, we perform a beam steering operation adopting a multibeam approach for both sensing and communication. Other methods exist in the literature for beamforming, e.g., based on optimization techniques, further improving performance \([15], [16]\).
Looking at (2), it is evident the trade-off between the performance of the communication and sensing functions. To guarantee certain sensing capabilities, it is necessary to reserve a fraction of the total power available for it, with a consequent reduction in communication coverage. To study how the communication system coverage changes by varying the EIRP, some metrics can be used according to the 3GPP Technical Report in [37]. In particular, maximum coupling loss (MCL), maximum path loss (MPL) and maximum isotropic loss (MIL) are the metrics used in 5G NR systems to express the coverage of the communication system [37], [38]. These metrics differ for some terms, but they share the main idea of maximum loss that the communication system can tolerate and still be operational. In particular, differently from MCL, MIL and MPL include also the antenna gains. Moreover, the MIL metric takes into account parameters such as shadow fading and penetration margins. A detailed analysis of this metric is out of the scope of this paper, but it is important to highlight that the fraction of power \( \rho \) reserved for sensing results in a reduction of MPL and MIL by a factor 10\( \log_{10}(\rho) \) dB.

**B. Received signal**

The vector \( \tilde{y}_k^{(m)} \in \mathbb{C}^{N_T \times 1} \) of the received modulation symbols at each antenna after the fast Fourier transform (FFT) block in the OFDM receiver, is given by

\[
\tilde{y}_k^{(m)} = H_k^{(m)} x_k^{(m)} + \nu_k^{(m)} + \tilde{n}_k
\]

(7)

where \( H_k^{(m)} \in \mathbb{C}^{N_T \times N_C} \) is the channel matrix for the \( m \)th OFDM symbol and the \( k \)th subcarrier, \( \nu_k^{(m)} \in \mathbb{C}^{N_T \times 1} \) is the vector whose elements represent the self interference (SI) due to imperfect Tx–Rx isolation at each receiving antenna, and \( \tilde{n}_k \in \mathbb{C}^{N_T \times 1} \) is the additive white Gaussian noise (AWGN) vector whose entries are independent, identically distributed (i.i.d.) random variables (r.v.s), having circularly symmetric zero mean Gaussian distribution with variance \( \sigma_N^2 \).

Considering \( L \) point target reflections, the channel matrix can be written as

\[
H_k^{(m)} = \sum_{l=1}^{L} \alpha_l e^{j2\pi m T_f \Delta f T_l} a_R(\theta_l) a_T(\theta_l)^	op
\]

(8)

where \( \theta_l, f_D, l, T_f \) and \( \theta \) are the round-trip delay, the Doppler shift, and the DoA of the \( l \)th target, respectively. The term \( \alpha_l = |\alpha_l| e^{j\phi_l} \) is the complex amplitude which includes phase shift and attenuation along the \( l \)th propagation path. The array response vector at the receiver for sensing is denoted in (8) by \( a_R(\theta_l) \). To simplify the presentation of the DoA estimation method, (8) can be recast in the more compact form

\[
H_k^{(m)} = A_R(\theta) \Sigma A_T(\theta)^	op
\]

(9)

where \( A_R(\theta) = [a_R(\theta_1), \ldots, a_R(\theta_L)] \in \mathbb{C}^{N_R \times L} \) and \( A_T(\theta) = [a_T(\theta_1), \ldots, a_T(\theta_L)] \in \mathbb{C}^{N_T \times L} \) are the steering matrices for the targets’ directions \( \theta = [\theta_1, \theta_2, \ldots, \theta_L] \), and \( \Sigma = \text{diag}(\beta_1, \beta_2, \ldots, \beta_L) \in \mathbb{C}^{L \times L} \) is the diagonal matrix of the channel coefficients.

For what concerns the SI term, \( \nu_k^{(m)} \), in (7), each element \( n \) of this vector can be considered as the signal scattered by a static target with an almost null distance from the receiver, i.e., with \( f_{D,Sl} = 0 \) and \( \tau_{Sl} = 0 \), thus it can be written as \( \nu_k^{(m)} = \alpha_{Sl,n} x_k^{(m)} \), where \( \alpha_{Sl,n} = |\alpha_{Sl,n}| e^{j\phi_{Sl,n}} \) is the complex amplitude, which includes phase shift and attenuation of the SI contribution at the \( n \)th receiving antenna element [6], [39]. As for the targets, all the attenuation factors \( \alpha_{Sl,n} \) are assumed to be the same for all the receiving antennas. Therefore, the signal-to-self interference ratio (SSIR) for the eco generated by the target \( l \) at each receiving antenna is given by

\[
\text{SSIR} = \frac{\|\alpha_l\|^2}{\|\alpha_{Sl,n}\|^2}.
\]

(10)

Starting from (7), by performing spatial combining through
the receiving BF vector, \(\mathbf{w}_R = a_R^\dagger(\theta_{R,s})\), we have the received symbol
\(y_k^{(m)} = \mathbf{w}_R^T x_k^{(m)}\), which, using (9), can be expressed as
\[y_k^{(m)} = \mathbf{w}_R^T A_R(\theta) \Sigma A_R^T(\theta) \mathbf{\hat{x}}_k^{(m)} + \mathbf{w}_R^T \mathbf{n}_k.\] (11)

C. Beam-scanning

As mentioned above, the considered system is a multibeam JSC scheme, with a beam pointing to the UE and a beam pointing sequentially to different directions to sense the environment.

Referring to Fig. 1 during a scan the DoD and the DoA for sensing are the same. Specifically, we have
\[\theta_{T,s} = \theta_{R,s} = \theta_0 + i \Delta \theta_s \quad i = 0, \ldots, N_{\text{dir}} - 1\] (12)
where \(\theta_0\) is the starting scan direction, \(\Delta \theta_s\) is the scan angle step, \(i\) is the index used to update the direction, and \(N_{\text{dir}}\) is the number of directions explored to perform a complete scan from \(-\theta_0\) to \(\theta_0\). For each sensing direction, a number of OFDM symbols \(M_s < M\) is acquired from the receiver system. Therefore, since a 5G NR frame with \(M\) symbols lasts \(T_s = 10\) ms, by fixing \(N_{\text{dir}}\) it is possible to determine the number of frames and the time required to complete a scan as:
\[N_f = \left\lfloor \frac{M_s N_{\text{dir}}}{M} \right\rfloor, \quad T_{\text{scan}} = T_s N_f.\] (13)

The OFDM symbols collected in each direction are used to estimate range, Doppler and DoA of the target.

D. Sensor-target-sensor path

In line-of-sight (LOS) propagation conditions the power received at a given array element from the \(l\)th path, illuminated by the sensing beam, is proportional to \(\alpha_l^2\) and given by
\[P_{R,l} = \rho \cdot \frac{P_T G_R^2 G_R e^{2\sigma_{\text{RCS},l}}}{(4\pi)^3 f^2 d^4} \cdot \gamma_l\] (14)
where \(\sigma_{\text{RCS},l}\) is the radar cross-section (RCS) of the point target \(l\), \(d_l\) is the distance between the \(l\)th target and the BS, \(G_R\) is the single element antenna gain at RX, and \(\gamma_l = |\text{AF}(\theta_{T,s} - \theta_l)|^2 \in [0, 1]\) where \(\text{AF}(\theta)\) is the normalized array factor at Tx that considers the non-perfect alignment between the target DoA and the sensing direction \(\theta_l\); when \(\theta_l = \theta_{T,s}\) then \(\gamma_l = 1\). The signal-to-noise ratio (SNR) at the single receiving antenna element related to the \(l\)th target is defined as
\[\text{SNR}_l = \frac{P_{R,l}}{N_0 K \Delta f}\] (15)
where \(P_{R,l}\), the received power from the \(l\)th path, is given in (14), and \(N_0\) is the one-sided noise power spectral density (PSD) at each antenna element. When convenient, by normalizing the received symbols after the FFT in the OFDM receiver as \(E\{|y_{n,k}^{(m)}|^2\} = 1\), (15) reduces to \(\text{SNR}_l = 1/\sigma_{\text{R}}^2\).

III. ESTIMATION OF TARGET PARAMETERS AND DETECTION

This section introduces MUltiple SIgnal Classification (MUSIC) for DoA estimation and periodogram-based frequency estimation for range and velocity evaluation. The estimation methods are performed for each sensing beam step in which \(M_s\) OFDM symbols are collected. To simplify the notation, we drop the scan index \(i\).

A. Estimation of the number of targets and DoAs

DoA estimation is performed by MUSIC that requires knowledge of the noise subspace, which in turn needs the number of targets to be known. Noise subspace can be identified via the covariance matrix of the received vector \(\mathbf{R} = \mathbb{E}\{\mathbf{y}_k^{(m)} \mathbf{y}_k^{(m)\dagger}\}\) in \(\mathbb{C}^{N_R \times N_R}\). In fact, since the noise is zero mean and independent of the target echoes, it follows that the \(N_R - L\) smallest eigenvalues of \(\mathbf{R}\) are all equal to the noise power \(\sigma_N^2\) and the corresponding eigenvectors identify the noise subspace. Since the covariance matrix is not known a priori, the sample covariance matrix (SCM) can be used instead \([32]\). It is given by
\[\hat{\mathbf{R}} = \frac{1}{KM_s} \sum_{m=0}^{M-1} \sum_{k=0}^{L-1} \mathbf{y}_k^{(m)} \mathbf{y}_k^{(m)\dagger}.\] (16)

The number of sources (target echoes in our scenario) can be estimated by model order selection based on information theoretic criteria \([41], [42]\). The approach starts by performing eigenvalue decomposition of the SCM of the observed vectors, \(\hat{\mathbf{R}} = \mathbf{U} \Lambda \mathbf{U}^\dagger\), where the columns of \(\mathbf{U} \in \mathbb{C}^{N_R \times N_R}\) are the eigenvectors and \(\Lambda = \text{diag}(\lambda_1, \ldots, \lambda_{N_R})\) is a diagonal matrix with eigenvalues sorted in descending order, i.e., \(\lambda_1 \geq \lambda_2 \geq \cdots \geq \lambda_{N_R}\). Using the minimum description length (MDL) criterion, the estimated number of targets (considering that we are illuminating only targets within the sensing beam in the \(l\)th direction) is
\[L_m = \arg \min_{s \in \{0, \ldots, N_R - 1\}} \{\text{MDL}(s)\}\] (17)
with
\[\text{MDL}(s) = -\ln \left( \frac{\prod_{i=s+1}^{N_R} \lambda_i^{(N_R-s)}}{\prod_{i=s+1}^{N_R} \lambda_i^{(N_R-s)}} \right)^{(N_R-s)K M_s} + \frac{1}{2} s (2N_R - s) \ln(K M_s).\] (18)

The MUSIC algorithm then starts from \(\hat{\mathbf{U}} \in \mathbb{C}^{N_R \times (N_R - L_m)}\), the submatrix containing the \(N_R - L_m\) eigenvectors corresponding to the smallest eigenvalues, \(\lambda_{L_m+1}, \ldots, \lambda_{N_R}\), where such eigenvectors represent a good approximation of the noise subspace. Next, the pseudo-spectrum function, whose peaks reveal the presence of incoming signals, can be obtained as \([43]\)
\[f_m(\theta) = \frac{1}{\|\hat{\mathbf{U}}^\dagger \mathbf{a}(\theta)\|^2}.\] (19)

The peak locations in \(f_m(\theta)\) are the DoA estimates \(\hat{\theta}\). However, as it will be better explained in Section V, in each sensing direction we search for a local maximum of (19) in a limited angle range \([\theta_{\text{min}}, \theta_{\text{max}}]\), which depends on the beamwidth of the array response. The DoA estimate in each direction is thus

\(^{3}\text{As required by MUSIC we consider } L < N_R, \text{ i.e., the number of targets is less than the number of sensing array elements.}\)
given by
\[ \hat{\theta} = \arg \max_{\theta \in [\theta_{\min}, \theta_{\max}]} \{ f_m(\theta) \}. \] (20)

B. Detection and range-Doppler estimation

For the range-Doppler profile evaluation, we start from the received symbols \( \mathbf{y} \) from which, by expanding the matrix multiplications, we obtain
\[
y^{(m)}_k = \left( \sum_{i=1}^{L} \beta_i \mathbf{Y}(\theta_{T,s}, \theta_{R,s}, \theta_l) \right) x^{(m)}_k + n_k \tag{21}
\]
where \( n_k = w_k x_k^{(m)} \) and \( \mathbf{Y}(\theta_{T,s}, \theta_{R,s}, \theta_l) \in \mathbb{C} \) is a factor which accounts for the gain due to the array response vector at Tx and Rx and the DoA of the target. Since the range and velocity of targets are embedded in \( \beta_i \), first, a division is performed to remove the unwanted data symbols \( \mathbf{g}^{(m)} = y_k / x_k^{(m)} \), which leads to
\[
g^{(m)}_k = \sum_{i=1}^{L} \alpha_i e^{j2\pi mT_s f_{d,i} + j2\pi f_{\nu} T_s} \mathbf{Y}(\theta_{T,s}, \theta_{R,s}, \theta_l) + \nu_k \tag{22}
\]
where \( \nu_k = n_k / x_k^{(m)} \). Note that (22) contains, for each target, two complex sinusoids whose frequencies are related to \( f_{d,i} \) and \( f_{\nu} \), while \( \alpha_i \) and \( \mathbf{Y}(\theta_{T,s}, \theta_{R,s}, \theta_l) \) are constant terms.

Starting from (22), a periodogram can be computed in order to estimate range and speed of the target as \[ 6, 44, 45 \]
\[
P(q, p) = \left( \sum_{k=0}^{K_p-1} \sum_{m=0}^{M_p-1} g^{(m)}_k e^{-j2\pi m \frac{q}{K_p}} e^{j2\pi p \frac{k}{M_p}} \right)^2 \tag{23}
\]
with \( q = 0, \ldots, K_p - 1 \) and \( p = 0, \ldots, M_p - 1 \), which consists of \( K \) FFTs of length \( M_p \) and \( M_s \) inverse fast Fourier transforms (IFFTs) of length \( K_p \). In this work, \( K_p > K \) is calculated as the next power of two of \( K \), whereas \( M_p > M_s \) is the next power of two of \( F_p \cdot M_s \), where \( F_p \) is the zero-padding factor to improve speed estimation resolution.

The periodogram (23) represents the range-Doppler map from which the first operation performed is target detection by a hypothesis test between \( H_0 \), where only noise is present, and \( H_1 \), which refers to the presence of the target, i.e.,
\[
\mathcal{P}(q, p) \overset{H_1}{\gtrless} \eta \tag{24}
\]
The threshold \( \eta \) is chosen to ensure a predefined false alarm probability \( \mathbb{P}_A \). When the sensing beamwidth is relatively small, only one target is likely to be present in a given sensing direction, and if the test (24) rejects the null hypothesis, it is easy to find the location of the peak in the periodogram
\[
(\hat{q}, \hat{p}) = \arg \max_{(q,p)} \{ \mathcal{P}(q, p) \} \tag{25}
\]
evaluate the distance and radial speed of the target as
\[
\hat{r} = \frac{\hat{q} c}{2\Delta f K_p}, \quad \hat{v} = \frac{\hat{p} c}{2 f_c T_s M_p}. \tag{26}
\]
The distance and velocity resolutions are intrinsic characteristics of the periodogram and only depend on the 5G NR parameters, i.e., number of OFDM symbols, number of active subcarriers, subcarrier spacing, and OFDM symbol duration, and are given by \[ 44, \text{Chapter 3} \]
\[
\Delta r = \frac{c}{2 \Delta f K_p}, \quad \Delta v = \frac{c}{2 f_c T_s M_p}. \tag{27}
\]

C. Pruning redundant target points

As explained above, the considered JSC system searches for a peak in the pseudo-spectrum \[ 19 \] and in the periodogram \[ 23 \] for each sensing direction for which the test \[ 24 \] chooses the hypothesis \( H_1 \). When a target is detected in a particular direction, it might be detected also in some adjacent directions when the periodogram \( \mathcal{P} \) is above threshold because of the beam sidelobes. These detected points are originated by the same target and are characterized by inaccurate DoA estimates. As it will be better quantified in Section \[ V \] this effect is due to the choice of searching the maximum of MUSIC pseudo-spectrum in a limited range, as in \[ 20 \], that reduces the computational cost of searching but may yield multiple detection points per target. To maintain the benefits of local search, we propose a method to thin out redundant target points (hereafter also referred to as repeated targets) that has proven effective.

First, all the collected peaks and estimates are organized in a matrix \( \mathbf{Z} \), whose rows are the vectors
\[
\mathbf{z}_i = \left[ \hat{r}_i, \hat{v}_i, \mathcal{P}(\hat{r}_i, \hat{v}_i), \hat{\theta}_i, f_m(\hat{\theta}_i) \right] \quad i = 1, \ldots, N_{\text{max}} \tag{28}
\]
where \( N_{\text{max}} \leq N_{\text{dir}} \) is the number of sensing directions in which the test \[ 24 \] rejects the null hypothesis. Subsequently, these rows are sorted in descending order with respect to the values, \( \mathcal{P}(\hat{r}_i, \hat{v}_i) \), to form a new matrix \( \mathbf{Z}_{\text{sort}} \). Finally,

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**Algorithm 1 Pruning redundant target points**

Require: \( \mathbf{Z} \leftarrow \mathbf{z}_i = [\hat{r}_i, \hat{v}_i, \mathcal{P}(\hat{r}_i, \hat{v}_i), \hat{\theta}_i, f_m(\hat{\theta}_i)] \)

1: \( \mathbf{Z}_{\text{sort}} \leftarrow \text{sort } \mathbf{Z} \text{ in decreasing order according to the 3rd column} \)
2: \( \mathbf{z}_{\text{prun},1} \leftarrow \mathbf{z}_{\text{sort},1} \) \quad \text{▷ copy first row of } \mathbf{Z}_{\text{sort}} \text{ in } \mathbf{Z}_{\text{prun}} \)
3: \( \mathbf{z}_1 \leftarrow 1 \quad \text{▷ initialize row index of } \mathbf{Z}_{\text{prun}} \)
4: \textbf{for } \( i = 2 : N_{\text{max}} \textbf{ do} \)
5: \( \text{count} \leftarrow 0 \)
6: \textbf{for } \( j = 1 : k \textbf{ do} \)
7: \( \text{if } \mathbf{z}_{\text{prun},j} - \epsilon_r \leq \mathbf{z}_{\text{sort},i} - \mathbf{z}_{\text{prun},j} + \epsilon_r \) \quad \text{and} \)
8: \( \hat{v}_{\text{prun},j} - \epsilon_v \leq \hat{v}_{\text{sort},i} \leq \hat{v}_{\text{prun},j} + \epsilon_v \) \textbf{ then} \)
9: \( \text{count} \leftarrow \text{count} + 1 \quad \text{break} \)
10: \textbf{end if} \)
11: \textbf{end for} \)
12: \textbf{end for} \)
13: \textbf{if } \text{count} = 0 \quad \textbf{ then} \)
14: \( \mathbf{z}_k \leftarrow k + 1 \) \quad \textbf{▷ update row index of } \mathbf{Z}_{\text{prun}} \)
15: \( \mathbf{z}_{\text{prun},k} \leftarrow \mathbf{z}_{\text{sort},i} \)
16: \textbf{end if} \)
17: \textbf{end for} \)
18: \( \mathbf{\hat{L}} \leftarrow k \)

Output: \( \mathbf{Z}_{\text{prun}} \) and its number of rows, \( \mathbf{\hat{L}} \)
a check on the elements of $Z_{\text{sort}}$ is performed to remove redundant target points, i.e., those with very similar estimates of both distance and radial velocity (within a given range of uncertainty). This results in a new matrix $Z_{\text{prun}}$ with a number of rows $\hat{L} \leq N_{\text{max}}$. The sort operation ensures that only range and speed pairs associated with the largest values of the periodogram are kept between the repeated points. The whole procedure is detailed in Algorithm [1]. As it can be seen, the definition of redundant target point is linked to the choice of two parameters, $\epsilon_r$, and $\epsilon_v$, that account for the measurement uncertainty. In particular, in the algorithm a target indexed with $i$ is considered a repetition of an already detected target denoted with $j$ if its estimated range, $\hat{r}_i$, and velocity, $\hat{v}_i$, meet the conditions, $\hat{r}_j - \epsilon_r \leq \hat{r}_i \leq \hat{r}_j + \epsilon_r$, and $\hat{v}_j - \epsilon_v \leq \hat{v}_i \leq \hat{v}_j + \epsilon_v$, respectively. The choice of the two parameters $\epsilon_r$ and $\epsilon_v$ will be discussed in Section V.

IV. PERFORMANCE EVALUATION IN THE PRESENCE OF MULTIPLE TARGETS

This section introduces the performance metric employed to address the concept of miss-distance, or error, in a multi-target system. In particular, when considering a multi-object system, a consistent metric should capture the difference between two sets of vectors (the truth and the estimated), not only in terms of localization error but also in terms of cardinality error. For this reason, in this work, the OSPA metric [46, 47] is used to study the performance of the considered JSC system in a multi-target scenario.

The OSPA metric is a miss-distance indicator, which summarizes in a unique measure the estimation accuracy in both the number and location of the targets. More precisely, given the true positions of the $L$ targets, $P = [p_1, \ldots, p_L]$, with $p_l = (x_l, y_l) = (r_l \cos \theta_l, r_l \sin \theta_l)$ and the $\hat{L}$ estimates, $\hat{P} = [\hat{p}_1, \ldots, \hat{p}_{\hat{L}}]$, the distance between an arbitrary pair of the estimate and the true position, cut off at $\bar{c} > 0$, is defined as [46]

$$d^{(\bar{c})} (P, \hat{P}) = \min \{ \bar{c}, d(P, \hat{P}) \}$$  \hspace{1cm} (29)

where $d(P, \hat{P}) = \| P - \hat{P} \|_2$ is the Euclidean distance between the estimate and the true position, and $\bar{c}$ is the cutoff parameter that determines how the metric penalizes cardinality error with respect to the localization one. Denoting by $\Pi_L$ the set of permutations on $\{1, 2, \ldots, k\}$ for any $k \in \mathbb{N}$, for $1 \leq q \leq \infty$ and $\bar{c} > 0$, the OSPA metric of order $q$ and with cutoff $\bar{c}$ is defined as [46]

$$d_q^{(\bar{c})} (P, \hat{P}) = \left( \frac{1}{\hat{L}} \min_{\pi \in \Pi_L} \sum_{l=1}^{\hat{L}} (d^{(\bar{c})} (P_l, \hat{P}_{\pi(l)}) )^q + \bar{c}^q (\hat{L} - L) \right)^{1/q}$$  \hspace{1cm} (30)

if $L \leq \hat{L}$, and $d_q^{(\bar{c})} (P, \hat{P}) = d_q^{(\bar{c})} (\hat{P}, P)$ if $L > \hat{L}$.

Essentially, for $L \leq \hat{L}$, the OSPA distance can be obtained by the following steps:

1) Find the $L$-elements subset of $\hat{P}$ that has the shortest distance to $P$, corresponding to the optimal subset assignment;

2) If a point $\hat{p}_n \in \hat{P}$ is not paired with any point in $P$, let $d_a = \bar{c}$; otherwise, $d_a$ is the minimum value between $\bar{c}$ and the distance between the two points in a pair;

3) The OSPA distance is given by $d_q^{(\bar{c})} (P, \hat{P}) = \left( \frac{1}{\hat{L}} \sum_{l=1}^{\hat{L}} d_q^{(\bar{c})} (P_l, \hat{P}_{\pi(l)}) \right)^{1/q}$, where $\Pi_L$ is the set of all permutations of $\{1, 2, \ldots, L\}$. The OSPA distance can be interpreted as a $q$th order per-target error for a multi-object scenario. The metric can be divided into two components, one accounting for localization error and the other for cardinality error. In particular, for $q < \infty$ these components are given by [46]

$$\epsilon_q^{(\bar{c})} (P, \hat{P}) = \left( \frac{1}{\hat{L}} \min_{\pi \in \Pi_L} \sum_{l=1}^{\hat{L}} (d^{(\bar{c})} (P_l, \hat{P}_{\pi(l)}) )^q \right)^{1/q},$$

$$\tilde{\epsilon}_q^{(\bar{c})} (P, \hat{P}) = \left( \frac{\bar{c}^q (\hat{L} - L)}{\hat{L}} \right)^{1/q},$$

if $L \leq \hat{L}$, and $\epsilon_q^{(\bar{c})} (P, \hat{P}) = \epsilon_q^{(\bar{c})} (\hat{P}, P)$, $\tilde{\epsilon}_q^{(\bar{c})} (P, \hat{P}) = \tilde{\epsilon}_q^{(\bar{c})} (\hat{P}, P)$ if $L > \hat{L}$.

In the metric, the value of $q$ determines the sensitivity of the $d_q^{(\bar{c})}$ to outlier estimates, while $\bar{c}$ balances the cardinality error component with respect to the localization one, as a part of the total error. As $\bar{c}$ decreases, the localization error becomes dominant compared with the cardinality error, whereas larger values of $\bar{c}$ emphasize the latter. The best choice for $\bar{c}$ to maintain a balance between the two components is any value significantly larger than a typical localization error, but significantly smaller than the maximum distance between objects.

V. SYSTEM-LEVEL ANALYSIS

System level analysis is carried out through numerical simulations to evaluate the performance of the above-described JSC scheme. For all the simulations, 5G NR signals compliant with 3GPP Technical Specification in [48] are considered. The main 5G NR parameters employed for the generation of the standardized signals are summarized in Table I. In addition, a

| TABLE I  
| JSC SYSTEM PARAMETERS |
|----------------------------------|
| 5G specification → | NR 100 | NR 400 |
| $f_c$ [GHz] | 3.5 | 28 |
| $\Delta f$ [kHz] | 30 | 120 |
| Active subcarriers $K$ | 3276 | 3168 |
| OFDM symbols per frame $M$ | 280 | 1120 |
| OFDM symbols per direction $M_c$ | 112 | 112 |
| Number of antennas $N_T = N_R$ | 10 | 10 |
| Array beamwidth $\Delta \Theta [^\circ]$ | 50 | 100 |

Note that $L$ is the estimated number of targets in our approach. This value may differ from $L_{\text{in}}$ given by [17] because the number of targets detected by MUSIC is conditioned on the considered sensing direction. After all, Tx beamforming performs spatial filtering, illuminating predominantly targets within the beamwidth.

4From now on, and without loss of generality, the monostatic sensor is considered at the origin of a Cartesian coordinate system.
The performance indicator to summarize the effectiveness of the designed system is the OSPA metric. The RMSE is computed for $q = 2$, as recommended by [46], and $c = 10$ m to guarantee a good balance between localization and cardinality error.

As it will be explained in the following, we will start investigating the impact of SI on estimation performance, focusing on the RMSE of DoA, distance, and speed estimates by varying the SSIR introduced in Section 1-B.

### A. RMSE and detection probability vs SNR and SSIR

Let us start analyzing the SI issue. Fig. 2 shows the RMSE of DoA, range, and radial speed estimates obtained when only a single target is present and SNR $= -20$ dB, by varying the SSIR for different 5G NR parameters and number of antennas. As it can be noticed, the system performance quickly degrades for low SSIR values, but when SSIR $\geq 10$ dB, the RMSE of DoA, range, and radial speed estimates, reaches a floor where thermal noise is the only limiting factor. Therefore, if proper SI suppression can be performed, either through beamforming optimization or through digital cancellation techniques [6], [32], the estimation error can be kept low.

From now on, an analysis of the RMSE by varying the SNR is performed considering SI negligible. In particular, the SNR is varied from $-65$ to $-15$ dB, while distance, speed, and DoA of the target are varied randomly, from one iteration to another, with a uniform distribution from 20 to 85 m, $-20$ to $20$ m/s, and $-60^\circ$ to $60^\circ$, respectively. In Fig. 3 the results obtained for the RMSE of distance, angle, speed, and position are shown. As the periodogram used to estimate speed and radial distance of the target is computed on the symbols obtained after spatial combining, the whole estimation process is subject to a double processing gain, one resulting from the periodogram calculation, equal to $10 \log_{10}(K \cdot M_s)$ dB [49], and the other from the beamforming gain, equal to $10 \log_{10}(N_R)$ dB. For this reason, the MIMO system can estimate range and speed with high accuracy for SNR significantly lower than those reached by the DoA estimation algorithm, as it can be seen in Fig. 4. In fact, MUSIC is not subject to any processing gain, and the RMSE of angle estimation starts to increase at much higher SNR values, depending on the number of receiving antennas, $N_R$.  

| SSIR [dB] | RMSE [m] |
|-----------|-----------|
| $-20$ dB  | $10^{-3}$ |
| $-15$ dB  | $10^{-2}$ |
| $-10$ dB  | $10^{-1}$ |
| $-5$ dB   | $10^{0}$  |
| $0$ dB    | $10^{1}$  |

| SSIR [°] | RMSE [m/s] |
|-----------|-------------|
| $-20$ dB  | $10^{-3}$   |
| $-15$ dB  | $10^{-2}$   |
| $-10$ dB  | $10^{-1}$   |
| $-5$ dB   | $10^{0}$    |
| $0$ dB    | $10^{1}$    |

Fig. 2. Sensing performance as a function of the SSIR for DoA, distance, and speed estimates, when SNR $= -20$ dB.
In particular, for increasingly negative values of SNR, the RMSE (in degree) vs SNR curves converge approximately to $\Delta \Theta/2.8$, because of the limited search interval, $\Delta \Theta$, over which the pseudo-spectrum is computed. As previously stated, $\Delta \Theta$, and consequently the upper bound value of the curves, strictly depends on the number of antennas, as it can be noticed comparing the blue dashed line and continuous yellow line curves in Fig. 3a, Fig. 3b and Fig. 3c.

From the estimated range, $\hat{r}$, and DoA, $\hat{\theta}$, the position estimate of the target is $\hat{\mathbf{p}} = (x, y) = (\hat{r} \cos \hat{\theta}, \hat{r} \sin \hat{\theta})$. The normalized RMSE, shown in Fig. 3d, is derived from the Euclidean distance between the estimated position, $\hat{\mathbf{p}}$, and the true location of the target, $\mathbf{p} = (x, y) = (r \cos \theta, r \sin \theta)$, divided by the true distance, $r$, as

$$\text{Normalized RMSE} = \sqrt{\frac{1}{N_{MC}} \sum_{j=1}^{N_{MC}} \frac{\| \hat{\mathbf{p}}_j - \mathbf{p}_j \|^2}{r_j^2}}. \quad (32)$$

The normalization in (32) eliminates the dependency of the position RMSE on the distance generalizing the results. In fact, since the length of the chord of a circumference is directly proportional to its radius, the DoA error causes the position error to increase with distance. In Fig. 3d the position estimate dependency on the DoA is emphasized for different numbers of antennas and 5G numerologies. As the SNR decreases, it is possible to notice the impact of DoA, which causes a first drop in the performance, and the effect of range estimation error, which leads to a second performance drop at lower SNR.

Another important parameter in sensing is the detection probability $P_D$ as a function of the SNR as shown in Fig. 3e. In these plots, the threshold $\eta$ has been chosen to ensure a $P_{FA} = 1\%$. As expected, since detection is performed on the range-Doppler map, the same map used for velocity and range estimation, it is easy to notice that the range and velocity estimation start degrading when detection probability degrades. Therefore, the main factor limiting the radar performance is DoA estimation.

**B. RMSE vs distance**

Let us now analyze the trade-off between communication and sensing varying $\rho$ in (2). As it can be observed in Fig. 4a and 4b, the system works well also for moderately low values of $\rho$, e.g., $\rho = 0.1$. Notably, the position RMSE is below 0.33 m and 0.1 m, at 3.5 GHz and 28 GHz, respectively, even at tens of meters (in LOS condition). It is also important to highlight that the RMSE values reached at 3.5 GHz are much higher than that at 28 GHz. This mainly depends on the larger $\Delta \Theta$ resulting from $N_T = N_R = 10$, with respect to the beamwidth with $N_T = N_R = 50$ antennas. Moreover,
C. Performance analysis of multi-target scenario

For the multi-object scenario analysis let us consider $L = 10$ point targets $(9 + 1 \text{ UE})$. Each target is associated with an SNR that depends on its radial distance from the monostatic sensor, on its RCS, and on the alignment between the target and the sensing direction, in accordance with (15). Without loss of generality let us assume all the targets with the same RCS, equal to $\sigma_{\text{RCS}} = 1 \text{ m}^2$, as in Section V-B. The number of MC iterations for this group of results is set to $N_{\text{MC}} = 500$. In each MC iteration targets positions are randomly generated according to a uniform distribution within a sector with radial distance between 20 to 85 m and angle from $-60^\circ$ to $60^\circ$.

The primary purpose of this analysis is to study the performance of the considered JSC system when multiple targets are present, computing the OSPA metric introduced in Section IV for different choices of $N_{\text{dir}}$, ranging from 30 to 60 sensing directions. In particular, one of the main objectives is to study the influence of the uncertainty parameters, $\epsilon_r$ and $\epsilon_v$, used in the repeated targets pruning algorithm presented in Section III-C and of the parameters $\rho$, on the detection and localization capabilities of the system.

For what concerns $\epsilon_r$ and $\epsilon_v$, a good choice consists of using a multiple of distance and velocity resolutions, $\Delta r$ and $\Delta v$, defined in (27). In fact, due to the presence of AWGN, radial distance and velocity estimates of a repeated target may fall in adjacent bins of the periodogram with respect to those of the original target. In this sense, between range and velocity, it is the latter that presents greater RMSE in the low SNR regime; this is due to zero padding, which increases velocity resolution at the expense of sensitivity to noise. The mean cardinality error is used to choose these parameters. This metric is given...
be regarded as approximately constant, so if $D$ decreases, that should be caused by a drop in the targets’ repetition rate. Fig. 5 shows the mean cardinality error and the mean OSPA metric is computed varying the number of sensing directions for different values of $\rho$, $\epsilon_r$ and $\rho_c$. The considered values are: $\epsilon_r = \Delta r$ and $\epsilon_v = 2\Delta v$ with $\rho = 0.1$ (a) and $\rho = 0.3$ (c), $\epsilon_r = \Delta r$ and $\epsilon_v = 3\Delta v$ with $\rho = 0.1$ (b) and $\rho = 0.3$ (d).

Importantly, this metric does not distinguish between miss-detection, false alarm, and repeated target; however, it can be considered a good indicator for analyzing the average performance of the considered algorithm. In fact, fixing the system parameters, miss-detection and false alarm rates can be considered as approximately constant, so if $D$ decreases, that should be caused by a drop in the targets’ repetition rate. Fig. 5 shows the mean cardinality error and the mean OSPA localization error computed varying the number of sensing directions, $N_{dir}$, for different values of $\epsilon_r$, $\epsilon_v$, and $\rho$. As it can clearly be noticed, by fixing $\epsilon_r$ and $\epsilon_v$, the overall performance of the system (both in localization and cardinality error) improves for increasing values of $\rho$. For what concerns the localization error, the results shown in Fig. 5 are in agreement with those presented in Fig. 4. As the position of the target is varied between 20 and 85 m, the system performance is worse for $\rho = 0.1$ than $\rho = 0.3$, as expected. In Fig. 5 it is possible to notice as for $N_{dir} \geq 40$ the mean cardinality error becomes smaller choosing $\epsilon_v = 3\Delta v$, both for $\rho = 0.3$ and $\rho = 0.1$, and, in particular, for $\rho = 0.3$ the system on average misses less than one target. As pointed out, a value of $\epsilon_r > \Delta r$ does not change appreciably the system performance; therefore, its value is kept fixed, letting $\epsilon_v$ vary. This latter term most affects the repeated targets pruning algorithm detection performance due to zero padding, as already observed.

In Fig. 6 the mean OSPA metric is computed varying $N_{dir}$ for the same values of $\epsilon_r$, $\epsilon_v$, and $\rho$ used above. In addition, the 20th and 80th percentile are shown to better understand the range of values the OSPA metric can assume for different positions of the targets. Also in this case, the best performance are obtained for $\rho = 0.3$, $\epsilon_r = \Delta r$ and $\epsilon_v = 3\Delta v$. In particular, for this choice of parameters the mean value of $d$ is below 3 m and the 20th percentile is approximately equal to 1 m for $N_{dir} = 60$. Note, however, that such numerical results also consider the portion of the monitored area where the DoA estimation is severely degraded (see Fig. 4), a proper sensing cell sizing may avoid such region and lead to much better performance.
of targets can be detected and localized with sub-meter level accuracy when the power for sensing is capable of ensuring reliable DoA estimation.

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VI. CONCLUSION

In this work, we designed a multibeam system for JSC based on 5G NR, capable of detecting and locating multiple targets. We provided a system-level analysis and proposed an algorithm for pruning phantom targets that arise as a consequence of beam-scanning in the presence of beam sidelobes. We identified the main dominant factors affecting performance and compared two system setups operating at sub-6 GHz, and mmWave frequencies. The findings of this paper have demonstrated that: i) DoA estimation is the primary source of error when used to evaluate the target position; ii) even with a relatively small fraction of power devoted to sensing, good localization performance at tens of meters can be achieved in LOS even at mmWave; iii) in the sub-6 GHz band targets can be detected at higher distances but with lower accuracy mainly because of the reduced number of antenna elements; iv) Tens of targets can be detected and localized with sub-meter level accuracy when the power for sensing is capable of ensuring reliable DoA estimation.
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