A Novel Modelling Approach of Modular Multi Three-phase Drive System for High Performance Applications

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Abstract—There is a growing attention in the industrial and academic sectors for the multi-phase drive for high power and high-speed applications. The multi three-phase drive with independent neutral points is a popular option for this application, as it allows for the usage of standard control and standard power electronics for the individual three-phase systems. This work presents a novel model of multi three phase drive. The mathematical modelling of multi three-phase permanent magnet synchronous machine (PMSM) and modular three-phase converters is presented. The electromagnetic torque equations of multi three-phase PMSM fed by modular converters are calculated. Finally, numerical results in a dual three-phase drive are presented to validate the analytical models.

Keywords—Analytical models, multi three-phase drive, torque control

I. INTRODUCTION

Multiphase drives have attracted an increasing attention for high speed and high power applications (e.g. aerospace applications) [1]–[3]. Among all multiphase drives, the multi three-phase drive (shown in Fig. 1) is one of the most popular option with its independent control of each three-phase subsystem [4]–[7]. In addition, commercial three-phase voltage source converters can be directly adopted to control the multi three-phase machines [8]–[10]. Therefore, modelling of multi three-phase drive systems is of high importance. Some research work has been done on the modelling of different drive systems [11]–[13]. This work is mainly focused on the mathematical modelling of multi three-phase Permanent Magnet Synchronous Machines (PMSMs) fed by voltage source Pulse Width Modulation (PWM) converters.

In section II, a mathematical model of multi three-phase PMSM is presented by analyzing the relationship between phase voltages and phase currents through the PMSM stator winding inductance matrix. Section III illustrates the mathematical model of the PWM converters by using double Fourier integral analysis method. Section IV calculates the electromagnetic torque of multi three-phase drives. The analytical models presented in Section II, III and IV are validated by numerical results in Section V. Finally, the conclusion of the paper is shown in Section VI.

II. MATHEMATICAL MODEL OF MULTI THREE-PHASE PMSM

The modelling of multi three-phase PMSM is based on the analysis of the relationship between phase voltages and currents. The inductance matrix, which establishes the relationship between phase currents and flux, allows for the calculation of the torque. While considering the self-inductance and mutual inductance of the inductance matrix of the PMSM, the effect of iron saturation is not considered, which means that the inductance value does not vary with the flux density. Assuming the self-inductance value on each stator phase \( a_1, b_1, c_1, \ldots, a_N, b_N, c_N \) are represented by \( l_{a_1a_1}, l_{b_1b_1}, l_{c_1c_1}, \ldots, l_{a_Na_N}, l_{b_Nb_N}, l_{c_Nc_N} \) respectively. Assuming the mutual-inductance value between phase \( a_1, b_1, c_1, \ldots, a_N, b_N, c_N \) are represented by \( M_{a_1b_1}, M_{a_1c_1}, \ldots, M_{c_Na_N}, M_{c_Nb_N} \) respectively. The inductance matrix table is a \( 3N \times 3N \) matrix table, which can be represented by:
Assuming $i$ and $j$ represent the $i$th row and the $j$th column of matrix $L$ respectively. Due to the mutual inductance theory, $M_{ij} = M_{ji}$, so matrix $L$ is a real symmetric matrix. The Matrix $L$ is strictly diagonally dominant matrix where $L_{ii} > \sum_{j=1,j \neq i}^N |L_{ij}|$ and $L_{ii} > 0$. Therefore, the inverse of matrix $L$ can be written as $L^{-1}$, and the determinant of matrix $L$ can be represented by $|L|$, and $|L| > 0$ [14].

The phase voltage is voltage drop between terminals $a_1$, $b_1$, $c_1$, ..., $a_N$, $b_N$, $c_N$ and terminal o, which can be represented by $u_{a1}, u_{b1}, u_{c1}, ..., u_{aN}, u_{bN}, u_{cN}$ respectively. The phase current is the current flowing through phase $a_1$, $b_1$, $c_1$, ..., $a_N$, $b_N$, $c_N$, which can be represented by $i_{a1}, i_{b1}, i_{c1}, ..., i_{aN}, i_{bN}, i_{cN}$ respectively. The resistance of each phase is $R$. The back-EMF generated on each phase is represented by $e_{a1}, e_{b1}, e_{c1}, ..., e_{aN}, e_{bN}, e_{cN}$ respectively. According to the electric principle, the phase voltage equation can be represented by (1):

$$
\begin{align*}
[u_{a1}] & = \begin{bmatrix} L_{a11} & L_{a12} & L_{a13} \\ L_{a21} & L_{a22} & L_{a23} \\ L_{a31} & L_{a32} & L_{a33} \\ \vdots & \vdots & \vdots \\ L_{N11} & L_{N12} & L_{N13} \\ L_{N21} & L_{N22} & L_{N23} \\ L_{N31} & L_{N32} & L_{N33} \\ \vdots & \vdots & \vdots \\ L_{N1N} & L_{N1N} & L_{N1N} \\ L_{N2N} & L_{N2N} & L_{N2N} \\ L_{N3N} & L_{N3N} & L_{N3N} \\ \vdots & \vdots & \vdots \\ L_{NNN} & L_{NNN} & L_{NNN} \end{bmatrix} \begin{bmatrix} i_{a1} \\ i_{b1} \\ i_{c1} \\ \vdots \\ i_{aN} \\ i_{bN} \\ i_{cN} \\ \vdots \\ i_{aN} \\ i_{bN} \\ i_{cN} \end{bmatrix} + R \begin{bmatrix} e_{a1} \\ e_{b1} \\ e_{c1} \\ \vdots \\ e_{aN} \\ e_{bN} \\ e_{cN} \\ \vdots \\ e_{aN} \\ e_{bN} \\ e_{cN} \end{bmatrix},
\end{align*}
\tag{1}
$$

simplified as:

$$
U = L \frac{d}{dt} I + RI + E.
\tag{2}
$$

with:

$$
\begin{align*}
U & = \begin{bmatrix} u_{a1} \\ u_{b1} \\ u_{c1} \\ u_{a2} \\ u_{b2} \\ u_{c2} \\ \vdots \\ u_{aN} \\ u_{bN} \\ u_{cN} \end{bmatrix},
I & = \begin{bmatrix} i_{a1} \\ i_{b1} \\ i_{c1} \\ \vdots \\ i_{aN} \\ i_{bN} \\ i_{cN} \end{bmatrix},
E & = \begin{bmatrix} e_{a1} \\ e_{b1} \\ e_{c1} \\ \vdots \\ e_{aN} \\ e_{bN} \\ e_{cN} \end{bmatrix},
\end{align*}
$$

Due to the symmetrical design principle of machine winding configurations, the inductance matrix table among multi three-phase systems $a_1$, $b_1$, $c_1$, ..., $a_N$, $b_N$, $c_N$ are identical, which means the inductance matrix $L_{pp} = L_{NN}$, $M_{pq} = M_{p+1,q+1}$, $M_{N,q} = M_{1,q+1}$, where $p \neq q, p, q \in \{1,2,...,N\}$, and:

$$
\begin{align*}
L_{pp} & = \begin{bmatrix} L_{a1p} & L_{a1p} & L_{a1p} \\ L_{b1p} & L_{b1p} & L_{b1p} \\ L_{c1p} & L_{c1p} & L_{c1p} \\ \vdots & \vdots & \vdots \\ L_{a1N} & L_{a1N} & L_{a1N} \\ L_{b1N} & L_{b1N} & L_{b1N} \\ L_{c1N} & L_{c1N} & L_{c1N} \end{bmatrix},
M_{pq} & = \begin{bmatrix} M_{a1p} & M_{a1q} & M_{a1q} \\ M_{b1p} & M_{b1q} & M_{b1q} \\ M_{c1p} & M_{c1q} & M_{c1q} \end{bmatrix},
\end{align*}
$$

Additionally, there is no phase displacements among different three-phase subsystems. Therefore, the back-EMFs generated on each phase are identical with the same magnitudes and phases, which means the back-EMF matrices $E_p = E_N$, where $p \in \{1,2,...,N\}$, and:

$$
\begin{align*}
E & = \begin{bmatrix} e_{a1} \\ e_{b1} \\ e_{c1} \\ \vdots \\ e_{aN} \\ e_{bN} \\ e_{cN} \end{bmatrix},
E_N & = \begin{bmatrix} e_{a1} \\ e_{b1} \\ e_{c1} \\ \vdots \\ e_{aN} \\ e_{bN} \\ e_{cN} \end{bmatrix}.
\end{align*}
$$

According to operational properties of matrices, (1) can be rewritten as:

$$
\begin{align*}
U_T & = L_t \frac{d}{dt} I_T + R I_T + E_T,
\end{align*}
\tag{4}
$$

simplified as:

$$
\begin{align*}
U_T & = L_t \frac{d}{dt} I_T + R I_T + E_T,
\end{align*}
\tag{5}
$$

Neglecting the harmonics caused by cogging effect and the shape permanent magnet, the back-EMF is considered to be ideal sinusoidal. Therefore, for $U_T$ and $I_T$, only the fundamental component, and the harmonic components, which are generated by PWM modulation effects, are considered. According to (5), the total equivalent fundamental voltage $U_f$, the total equivalent fundamental current $I_f$, the total equivalent harmonic voltage $U_h$ and the total equivalent harmonic current $I_h$ can be represented as:

$$
\begin{align*}
U_T & = U_f + U_h \\
I_T & = I_f + I_h \\
U_f & = (sL_T + R)I_f + E_T \\
U_h & = (sL_T + R)I_h
\end{align*}
\tag{6}
$$

with:

$$
\begin{align*}
U_f & = \begin{bmatrix} u_{a1f} \\ u_{b1f} \\ u_{c1f} \end{bmatrix},
I_f & = \begin{bmatrix} i_{a1f} \\ i_{b1f} \\ i_{c1f} \end{bmatrix},
U_h & = \begin{bmatrix} u_{ah} \\ u_{bh} \\ u_{ch} \end{bmatrix},
I_h & = \begin{bmatrix} i_{ah} \\ i_{bh} \\ i_{ch} \end{bmatrix}.
\end{align*}
$$
According to (6), by using Laplace formula, neglecting the initial conditions, $I_n$ can be represented as:

$$I_n = B(s)U_h,$$  
(7)

with:

$$B(s) = \begin{bmatrix} B_1(s) & B_2(s) & B_3(s) \\ B_4(s) & B_5(s) & B_6(s) \end{bmatrix}.$$  

It can be seen that all the elements in the matrix $B(s)$ including $B_1(s), B_2(s), B_3(s), B_4(s), B_5(s), B_6(s)$ can be represented by $B_l(s)$:

$$B_l(s) = \frac{C_{il}^2 + C_{ilh} + C_{ilh}^2}{C_{il} + C_{ilh} + C_{ilh}^2 + C_{lh}} ,$$

where $l \in \{1,2,3,4,5,6\}; C_{il}, C_{ilh}, C_{ilh}, C_{ilh}, C_{ilh}, C_{lh}$ are constants for any value of $l$. Therefore, referring to the formula of $B_l(s)$, it can be seen that $B_1(s), B_2(s), B_3(s), B_4(s), B_5(s), B_6(s)$ are low-pass filters. The relationship between the total equivalent harmonic current $i_{ch}$ and the total equivalent harmonic voltage $u_{ah}, u_{bh}, u_{ch}$ can be represented as:

$$\begin{cases} i_{ah} = B_1(s)u_{ah} + B_2(s)u_{bh} + B_3(s)u_{ch} \\ i_{bh} = B_4(s)u_{ah} + B_5(s)u_{bh} + B_6(s)u_{ch} \\ i_{ch} = B_1(s)u_{ah} + B_2(s)u_{bh} + B_3(s)u_{ch} \end{cases}.$$  
(8)

According to (8), the total equivalent current harmonics $i_{ah}, i_{bh}, i_{ch}$ are considered to be generated by the total equivalent harmonic voltages $u_{ah}, u_{bh}, u_{ch}$ through low-pass filters (i.e. the resistance-inductance network $B_l(s)$). The cancellation of phase voltage harmonic components may result in the cancellation of phase current harmonic components. Section IV shows that the major torque ripple is caused by the total equivalent harmonic currents. Thus, the working principle of the proposed torque ripple reduction method is based on the cancellation of total equivalent harmonic voltage harmonic voltages. Considering the low pass filter effect of the relationship between total equivalent harmonic voltage and current and the undesired effect of low order harmonics in electric machine systems, the lower order harmonic voltage is of first importance to be eliminated.

### III. MATHEMATICAL MODEL OF MODULAR PWM CONVERTERS

For double-edge naturally sampled pulse width modulation, the complete harmonic components can be solved by using double flourier integral analysis method [15], and the phase leg voltage $V_{\text{phase}}$ can be represented by:

$$u_{\text{phase}}(t) = \sum_{m=1}^{\infty} \sum_{n=-\infty}^{\infty} A_{mn} \cos(mx + ny).$$  
(13)

### IV. ELECTROMAGNETIC TORQUE CALCULATION

The electromagnetic torque of multi three-phase PMSM can be represented by:

$$T_e = \frac{1}{\omega_m} I^T \cdot E$$

$$= \frac{1}{\omega_m} \begin{bmatrix} i_{a1} & i_{b1} & i_{c1} & \ldots & i_{aN} & i_{bN} & i_{cN} \end{bmatrix} \begin{bmatrix} e_{a1} \\ e_{b1} \\ e_{c1} \\ \vdots \\ e_{aN} \\ e_{bN} \\ e_{cN} \end{bmatrix},$$  
(14)

where $\omega_m$ is the mechanical speed of the machine. Since $E_p = E_N$ for $p \in \{1,2,\ldots,N\}$, (14) can be rewritten as:

$$T_e = \frac{1}{\omega_m} \begin{bmatrix} i_{aT} & i_{bT} & i_{cT} \end{bmatrix} \begin{bmatrix} e_{aN} \\ e_{bN} \\ e_{cN} \end{bmatrix}.$$  
(15)

According to (15), the electromagnetic torque ripple can be represented as:

$$T_{e,ch} = \frac{1}{\omega_m} \begin{bmatrix} i_{ah} & i_{bh} & i_{ch} \end{bmatrix} \begin{bmatrix} e_{aN} \\ e_{bN} \\ e_{cN} \end{bmatrix}.$$  
(16)

According to (16), as only the fundamental component of the back-EMF is considered, the torque ripple is related to the total equivalent harmonic current $i_{ah}, i_{bh}, i_{ch}. As it has been discussed in the Section II that the cancellation of phase voltage harmonic components may result in the cancellation of current harmonic components. Therefore, the working principle of the proposed torque ripple reduction method is based on the cancellation of total equivalent harmonic voltages.

### V. ANALYTICAL AND SIMULATION RESULTS

Both analytical and the numerical results are obtained in order to the validate the mathematical models in Section II, III and IV. The analytical and numerical results are carried out based on a same dual three-phase drive with its converter and machine parameters listed in Table I. Analytical results are calculated based on (4), (9) and (15). The numerical results are obtained in PLECS with fixed time step of 0.01us. Fig. 2, Fig. 3 and Fig. 4 show the phase voltage, phase current and electromagnetic torque waveforms and their corresponding FFT spectra of the dual three-phase machine in both analytical and numerical results. According to Fig. 2, Fig. 3 and Fig. 4, the analytical results match with numerical

### TABLE I

| Parameter | Value |
|-----------|-------|
| DC link voltage ($V_{dc}$) | 500 [V] |
| Switching frequency ($f_s$) | 20 [kHz] |
| Modulating frequency ($f_m$) | 1 [kHz] |
| Rated power | 160 [kw] |
| Rated current | 280 [A] |
| Pole pair number | 3 |
| Phase resistance ($R$) | 11.47 [mΩ] |
| Mechanical speed ($\omega_{mech}$) | 2000 [rpm] |
| Stator phase inductance | 25 [μH] |
| Back-EMF coefficient ($K_e$) | 0.12 (phase peak back-EMF is 248V at 100Hz) |
results in general. The phase voltage waveforms of Fig. 2a
and Fig.2b are slightly different, as the numerical result is
obtained with infinite number of carrier signal index m
and infinite number of modulating signal index n. However, the
analytical result is obtained with limited number of carrier
signal index m (m=10) and limited number of modulating
signal index n (n=10) in MATLAB. This means that the
higher order phase voltage harmonic components are not
considered in the analytical results. The lower order phase
voltage harmonic components in the analytical result match
with the harmonic components in the numerical result, which
is shown in Fig. 2c and Fig. 2d. There is no obvious difference
between Fig. 3a (Fi. 4a) and Fig. 3b (Fig. 4b), as the phase
currents (electromagnetic torque) are generated by phase
voltages through low pass filters, mentioned in Section II and
Section IV, which indicates that the higher order phase
voltage harmonic components have less effect on the phase
currents and electromagnetic torque.

VI. CONCLUSION

This work proposes a method of modelling multi three-
phase drive. The models of multi three-phase PMSM and
voltage source PWM converter have been presented. The
electromagnetic torque equations of the multi three-phase
PMSM fed by modular voltage source PWM converters have
been calculated. Numerical results validate the analytical
models of a dual three-phase PMSM, voltage source PWM
converters and electromagnetic torque equations respectively.
It illustrates that the higher order phase voltage harmonic
components have less effect on the phase currents and
electromagnetic torque by comparing the numerical and
analytical results.

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