Concurrent Quad-band Low Noise Amplifier (QB-LNA) using Multisection Impedance Transformer

Teguh Firmansyah, Anggoro Suryo Pramudyono, Siswo Wardoyo, Romi Wiryadinata, Alimuddin
Department of Electrical Engineering, University of Sultan Ageng Tirtayasa, Indonesia

ABSTRACT

A quad-band low noise amplifier (QB-LNA) based on multisection impedance transformer designed and evaluated in this research. As a novelty, a multisection impedance transformer was used to produce QB-LNA. A multisection impedance transformer is used as input and output impedance matching because it has higher stability, large Q factor, and low noise than lumped component. The QB-LNA was designed on FR4 microstrip substrate with εr= 4.4, thickness h=1.6 mm, and tan δ= 0.026. The proposed QB-LNA was designed and analyzed by Advanced Design System (ADS). The simulation has shown that QB-LNA achieves gain (S21) of 22.91 dB, 16.5 dB, 11.18 dB, and 7.25 dB at 0.92 GHz, 1.84 GHz, 2.61 GHz, and 3.54 GHz, respectively. The QB-LNA obtains return loss (S11) of -21.28 dB, -31.87 dB, -28.08 dB, and -30.85 dB at 0.92 GHz, 1.84 GHz, 2.61 GHz, and 3.54 GHz, respectively. It also achieves a Noise figure (NF) of 2.35 dB, 2.13 dB, 2.56 dB, and 3.55 dB at 0.92 GHz, 1.84 GHz, 2.61 GHz, and 3.54 GHz, respectively. This research also has shown that the Figure of merit (FoM) of the proposed QB-LNA is higher than that of another multiband LNA.

1. INTRODUCTION

High demand for various types of wireless communications, encourage the research and development of multiband transceiver [1]. The multiband transceiver accommodate multiple types of wireless technologies simultaneously, making it cheaper, more efficient, and compact [2]. A subsystem of multiband transceiver consists of a multiband antenna (MA) [3], [4], a multiband power amplifier (MPA) [5], [6], a multiband mixer (MM) [7], a multiband band-pass filter (MBPF) [8-10] and multiband low noise amplifier (MLNA) [11-13]. A low noise amplifier (LNA) is necessary to amplify a signal without increasing the noise and interference at several frequencies simultaneously [14].

There are several method frequently used for MLNA design such as; wideband matching [15], switch method [16], and concurrent multiband [17-19]. The wideband method can produce LNA with wide frequency operating. However, this method has drawbacks such as high interference signal, because the unneeded signal is also strengthened. Meanwhile, switch method has the advantage of low interference but a switch-LNA works optimally at a single frequency. In addition, the switch method also requires additional switch with a good performance. A concurrent method could produce LNA with low interference and good performance at multiple frequencies simultaneously. The employment of concurrent multiband can be done by using lumped components as input and output matching impedances, but it makes the design of MLNA be more complex.

As novelty, a concurrent quad-band low noise amplifier (QB-LNA) using multisection impedance transformer was proposed in this paper. A multisection impedance transformer (MIT) was used to produce a
multiband matching circuit. MIT has many advantages including low noise, high stability, simple, and easy in fabrication. The QB-LNA has frequencies 0.92 GHz, 1.84 GHz, 2.61 GHz, and 3.54 GHz, for GSM900, WCDMA1800, LTE2600, and LTE3500 application respectively. The QB-LNA was designed on FR4 microstrip substrate with \( \varepsilon_r = 4.4, h = 1.6 \text{ mm} \), and tan \( \delta = 0.0265 \). The QB-LNA was simulated by using Schematic Simulation Advanced System Design (ADS). This research also was shown that the Figure of merit (FoM) of the proposed QB-LNA is higher than that of another multiband LNA.

2. THE PROPOSED METHOD

A subsystem of QB-LNA consist of bias transistor, input impedance matching (IIM), and output impedance matching (OIM) [12], [14] as shown in Figure 1. The FET NE321S01 with a low power source of bias \( V_{CC} = 5 \text{ V} \) was used. A multi-section impedance transformer (MIT) as IIM and OIM was proposed in this research to produce four-band LNAs as shown in Figure 2.

![Figure 1. A subsystem of multiband LNA](image1)

with termination port (R_s and R_L), bias circuit resistance R_N (N=1,2,3), power supply (V_CC), coupling capacitor C_N (N=1,2,3), RF choke (L_1), the impedance of transmission line \( Z_N \) (N=1,2,3,4,5,6,7,8,9), electrical length \( \theta_N \) (N=1,2,3,4,5,6,7,8,9), and input impedance \( Z_{IN} \).

2.1. Small Signal and Resonant Conditions Analysis

Figure 3 shows a small signal analysis of transistor bias circuit. The input impedance \( Z_{IN} \) is given by Equation (1) with transconductance \( g_m \), source inductance \( L_s \), gate inductance \( L_G \), and gate-source capacitance \( C_{GS} \).
\[ Z_{IN} = j\omega L_s + j\omega^2 C_{gs} + \frac{1}{j\omega C_{gs}} + \frac{g_m}{C_{gs}} L_s \]
\[ = j\omega (L_s + L_g) + \frac{1}{j\omega C_{gs}} + \frac{g_m}{C_{gs}} L_s \]

(1)

\[ Z_{IN} = j\omega (L_s + L_g) + \frac{1}{j\omega C_{gs}} + \omega_T L_s \]

(2)

A relation of cutoff frequency and transconductance is given by:
\[ \frac{g_m}{C_{gs}} L_s = \omega_T L_s \quad \rightarrow \quad \frac{g_m}{C_{gs}} = \omega_T \]

and \( Z_{IN} \) at cutoff frequency is given by:
\[ Z_{IN} = j\omega (L_s + L_g) + \frac{1}{j\omega C_{gs}} + \omega_T L_s \]

(3)

At a resonant frequency, the \( Z_{IN} \) can be found as follows:
\[ Im (Z_{IN}) = 0 \]

(4)

\[ Re (Z_{IN}) = \frac{g_m}{C_{gs}} L_s \]

(5)

At matching condition, \( Z_{IN} \) and return loss are given by:
\[ Z_{IN} = Z_s^* = R_S = \frac{g_m}{C_{gs}} L_s = \omega_T L_s \]

(6)

\[ S_{11} = \frac{Z_{IN}-R_S}{Z_{IN}+R_S} = \frac{(j\omega (L_s+L_g) + \frac{1}{j\omega C_{gs}} + \frac{g_m}{C_{gs}})}{(j\omega (L_s+L_g) + \frac{1}{j\omega C_{gs}} + \frac{g_m}{C_{gs}})} \]

\[ = \frac{\omega_T (L_s+L_g) + \frac{g_m}{C_{gs}}}{\omega_T (L_s+L_g) + \frac{g_m}{C_{gs}}} \]

\[ = \frac{(j\omega)^2 + \frac{g_m}{C_{gs}(L_s+L_g)}}{(j\omega)^2 + \frac{g_m}{C_{gs}(L_s+L_g)}} \]

(7)

With \( j\omega = \text{sat resonant frequency (}\omega_0\text{)} \), the Equation (7) could be simplified;
\[ S_{11} = \frac{s^2 + \omega_0^2}{s^2 + B_S + \omega_0^2} \]

(8)

With

Figure 3. Small signal analysis of bias circuit
\[
\omega_0^2 = \frac{1}{C_{gs}(L_s + L_g)} \\
B = 2 \frac{1}{(L_s + L_g) C_{gs} L_s}
\]

A bandwidth of LNA could be found at \( S_{11} \) lower than -10 dB, the \( S_{11} \) is formulated by:

\[
20 \log |S_{11}| \leq -10 \text{ dB} \\
\log |S_{11}| \leq -0.5 \\
|S_{11}| \leq 3.16
\]  \hspace{1cm} (9)

The upper and lower threshold is followed by:

\[
\frac{-B + \sqrt{B^2 + 4\omega_0^2}}{2} \leq \omega \leq \frac{B + \sqrt{B^2 + 4\omega_0^2}}{2}
\]  \hspace{1cm} (10)

2.2. Single-section Impedance Transformer (SIT)

Figure 4 shows a single section impedance transformer.

![Single-section Impedance Transformer](image)

Figure 4. Single-section Impedance Transformer

The partial reflection coefficients \( \Gamma_N \) (N=1,2,3) and partial transmission coefficients \( T_N \) (N=1,2) are given by:

\[
\Gamma_1 = \frac{Z_2 - Z_1}{Z_2 + Z_1}
\]  \hspace{1cm} (11)

\[
\Gamma_2 = -\Gamma_1
\]  \hspace{1cm} (12)

\[
\Gamma_3 = \frac{Z_3 - Z_2}{Z_3 + Z_2}
\]  \hspace{1cm} (13)

\[
T_{21} = 1 + \Gamma_1 = \frac{2Z_2}{Z_1 + Z_2}
\]  \hspace{1cm} (14)

\[
T_{12} = 1 + \Gamma_2 = \frac{2Z_2}{Z_2 + Z_2}
\]  \hspace{1cm} (15)

A total reflection can be calculated as follows:

\[
\Gamma = \Gamma_1 + T_{12} T_{21} e^{-2j\theta} \sum_{n=0}^{\infty} \Gamma_2^n e^{-2j\theta}
\]  \hspace{1cm} (16)

A geometry series was used for simplifying Equation (16), then the total reflection can be found:

\[
\Gamma = \Gamma_1 + \frac{T_{12} T_{21} e^{-2j\theta}}{1 - \Gamma_2 e^{-2j\theta}}
\]  \hspace{1cm} (17)
2.3. Multi-section Impedance Transformer (MIT)

To produce QB-LNA with quad-band impedance matching circuit at IMM and OIM, a multisection impedance transformer (MIT) was used, as shown in Figure 5. MIT has many advantages including low noise, high stability, simple, and easy in fabrication. The \( Z_{\text{IN}} \) is given by (18) with \( i = 1, \ldots, M \), propagations constant \((\beta_i)\), and electrical length \((l_i)\).

\[
Z'_i = Z_1 \frac{Z_{i+1} + j Z_i \tan(\beta l_i)}{Z_i + Z_{i+1} \tan(\beta l_i)}
\]  

\( \beta = \frac{\ell}{l_0}, \theta = \tan^{-1} \left( \frac{\beta}{\ell} \right) \)

(18)

![Figure 5. Multisection impedance transformer](image)

with low frequency dispersion and \( \theta(f) = \frac{f}{f_0} \theta_0 \), input impedance \((Z'_1)\) is given by:

\[
Z'_1 = Z_1 \frac{Z_{2} + j Z_1 \tan(\frac{f l_1}{f_0})}{Z_1 + Z_2 \tan(\frac{f l_1}{f_0})}
\]

(19)

At matching condition, return loss is given by:

\[
\left\{ \begin{array}{l}
\Gamma\left(\frac{l_1}{l_0}, \theta_0, Z_L(f), Z_1, Z_2, \ldots, Z_M\right)_{f=f_1} = 0 \\
\Gamma\left(\frac{l_2}{l_0}, \theta_0, Z_L(f), Z_1, Z_2, \ldots, Z_M\right)_{f=f_2} = 0 \\
\vdots \\
\Gamma\left(\frac{l_N}{l_0}, \theta_0, Z_L(f), Z_1, Z_2, \ldots, Z_M\right)_{f=f_N} = 0
\end{array} \right.
\]

(20)

3. DESIGN AND SIMULATION

To show the applicability of proposed concept of QB-LNA, a multisection impedance transformer (MIT) was used as shown in Figure 6. The QB-LNA has been designed with frequencies 0.92 GHz, 1.84 GHz, 2.61 GHz, and 3.54 GHz for GSM900, WCDMA1800, LTE2600, and LTE3500 application respectively. The QB-LNA was designed on FR4 microstrip substrate with \( \epsilon_r = 4.4, h=1.6 \) mm, and \( \tan \delta = 0.0265 \). The width and length of transmission line are \( w_1 = 22.4 \) mm, \( w_2 = 15.4 \) mm, \( w_3 = 6.3 \) mm, \( w_4 = 1.6 \) mm, \( w_5 = 0.3 \) mm, \( w_6 = 2.0 \) mm, \( w_7 = 1.0 \) mm, \( w_8 = 3.0 \) mm, \( w_9 = 1.0 \) mm and \( l_1 = 23.8 \) mm, \( l_2 = 8.1 \) mm, \( l_3 = 12.56 \) mm, \( l_4 = 18 \) mm, \( l_5 = 21 \) mm, \( l_6 = 0.3 \) mm, \( l_7 = 0.5 \) mm, \( l_8 = 20 \) mm, \( l_9 = 20 \) mm. The lumped components \( V_{cc} = 5 \) V, \( L_1 = 47 \) nH (as a RF Choke), \( R_1 = 475 \) \( \Omega \), \( R_2 = 3 \) k\( \Omega \), \( R_3 = 51 \) \( \Omega \), \( C_3 = 30 \) pF, \( R_S = 50 \) \( \Omega \) (as a input termination), and \( R_L = 50 \) \( \Omega \) (as a output termination).
Figure 6. QB-LNA using multisection impedance transformer (MIT)

Figure 7. (a) The extracted center frequency with varied \( \frac{w_4}{w_3} \), (b) the extracted of return loss \( (S_{11}) \) with varied \( \frac{w_4}{w_3} \), (c) the extracted of gain \( (S_{21}) \) with varied \( \frac{w_4}{w_3} \)

The extracted center frequency with varied \( \frac{w_4}{w_3} \), a return loss \( (S_{11}) \) with varied \( \frac{w_4}{w_3} \), gain \( (S_{21}) \) with varied \( \frac{w_4}{w_3} \), are shown in Figure 7(a), 7(b), and 7(c), respectively. Figure 7(a) shows that the center frequency of \( f_1 \), \( f_3 \), and \( f_4 \) are still stable with varied \( \frac{w_4}{w_3} \). However, a return loss \( (S_{11}) \) of \( f_2 \) has decreased as shown in Figure 7(b). Figure 7(b) shows that the increase of \( \frac{w_4}{w_3} \) would effect to the return loss \( (S_{11}) \). Figure 7(c) illustrated the extraction of gain \( (S_{21}) \) with varied \( \frac{w_4}{w_3} \). It shows that gain \( (S_{21}) \) of frequency \( f_1 \), \( f_3 \), and \( f_4 \) vary slightly, but a gain at frequency of \( f_1 \) falls dramatically. In general, the variation of \( \frac{w_4}{w_3} \) only affects the performances of the second frequency \( (f_2) \), but it does slightly affect to performances of frequency \( f_1 \), \( f_3 \), and \( f_4 \).
Figure 8(a) and 8(b) show the extracted return loss ($S_{11}$) and gain ($S_{21}$) with varied power supply ($V_{CC}$). It is useful for demonstrating the consistency performance of QB-LNA. The return loss ($S_{11}$) of frequency $f_1$, $f_2$, $f_3$, and $f_4$ remains constant. However, the value of gain ($S_{21}$) and Noise figure (nf) shifted because a varied of power supply ($V_{CC}$).

Figure 8. (a) The extracted of return loss ($S_{11}$) and gain ($S_{21}$), (b) Noise figure with varied $V_{CC}$

Figure 9 (a) shows the extracted return loss ($S_{11}$) and gain ($S_{21}$) with varied $l_1$. The chart shows that a return loss ($S_{11}$) and gain ($S_{21}$) of $f_1$ has not changed. However, the center frequency of $f_2$, $f_3$, and $f_4$ are shifted by varied of $l_1$. Figure 9(b) shows the extracted return loss ($S_{11}$) and gain ($S_{21}$) with varied $w_2$. The results are similar, a return loss ($S_{11}$) of $f_1$ has not changed and the center frequency of $f_2$, $f_3$, and $f_4$ are shifted because variation of $w_2$.

Figure 9. (a) The extracted return loss ($S_{11}$) and gain ($S_{21}$) with varied $l_1$ (b). The extracted return loss ($S_{11}$) and gain ($S_{21}$) with varied $w_2$

4. RESULTS AND ANALYSIS

The QB-LNA was designed on FR4 microstrip substrate with $\epsilon_r=4.4$, thickness $h=1.6$ mm, and tan $\delta=0.026$. The proposed QB-LNA was designed and analyzed by Advanced System Design (ADS). Figure 10 shows the performance of return loss ($S_{11}$) and gain ($S_{21}$) of QB-LNA.

The simulation has shown that QB-LNA achieves gain ($S_{21}$) of 22.91 dB, 16.5 dB, 11.18 dB, and 7.25 dB at 0.92 GHz, 1.84 GHz, 2.61 GHz, and 3.54 GHz, respectively. The QB-LNA obtain return loss ($S_{11}$)
of -21.28 dB, -31.87 dB, -28.08 dB, and -30.85 dB at 0.92 GHz, 1.84 GHz, 2.61 GHz, and 3.54 GHz, respectively. Figure 11 shows the performance of Noise figure (dB) and stability factor (K) of QB-LNA. This QB-LNA achieves a Noise figure (nf) of 2.35 dB, 2.13 dB, 2.56 dB, and 3.55 dB at 0.92 GHz, 1.84 GHz, 2.61 GHz, and 3.54 GHz, respectively. Furthermore, the stability factor of all bands above 1.0 is also depicted in Figure 11.

![Figure 10. The performance of return loss (S11) and gain (S21) of QB-LNA](image1)

![Figure 11. The performance of Noise figure (dB) and stability factor (K) of QB-LNA](image2)

This research has shown that the Figure of merit (FoM) of the proposed QB-LNA is higher than another multiband LNA, as shown in Table 1. A FoM is given by [20]

$$\text{FoM [mW}^{-1}\text{]} = \frac{\text{Gain [abs]}}{\text{(NF-1)[abs]P_{DC}[mW]}}$$  \hspace{1cm} (21)

| Parameter | Reference [17] | Reference [18] | Reference [19] | This work |
|-----------|----------------|----------------|----------------|------------|
| $f_0$ (GHz) | 1.80 | 2.45 | 2.40 | 5.20 | 2.20 | 4.60 | 0.92 | 1.84 | 2.61 | 3.54 |
| $S_{21}$ (dB) | 9.20 | 12.00 | 15.00 | 6.50 | 10.80 | 8.80 | 22.91 | 16.5 | 11.18 | 7.25 |
| NF (dB) | 5.70 | 6.40 | 2.50 | 2.40 | 3.53 | 2.52 | 2.35 | 2.13 | 2.56 | 3.55 |
| $P_{DC}$ (mW) | 8.00 | 10 | 7.76 | 5.01 |
| Gain/ $P_{DC}$ (dB/mW) | 1.15 | 1.50 | 1.50 | 0.65 | 1.38 | 1.13 | 4.51 | 3.29 | 2.23 | 1.44 |
| FoM (mW$^{-1}$) | 0.38 | 0.59 | 4.07 | 0.61 | 1.21 | 1.24 | 3.34 | 2.91 | 1.44 | 0.56 |

5. CONCLUSION

A multisection impedance transformer was used to produce QB-LNA. The QB-LNA has been designed with frequencies 0.92 GHz, 1.84 GHz, 2.61 GHz, and 3.54 GHz, for GSM900, WCDMA1800, LTE2600, and LTE3500 application respectively. The QB-LNA was designed on FR4 microstrip substrate with εr= 4.4, thickness h=1.6 mm, and tan δ= 0.026. The proposed QB-LNA was designed and analyzed by Advanced System Design (ADS). The simulation has shown that QB-LNA achieves gain ($S_{21}$) of 22.91 dB, 16.5 dB, 11.18 dB, and 7.25 dB at 0.92 GHz, 1.84 GHz, 2.61 GHz, and 3.54 GHz, respectively. The QB-LNA obtains return loss ($S_{11}$) of -21.28 dB, -31.87 dB, -28.08 dB, and -30.85 dB at 0.92 GHz, 1.84 GHz, 2.61 GHz, and 3.54 GHz, respectively. It also achieves a Noise figure (nf) of 2.35 dB, 2.13 dB, 2.56 dB, and 3.55 dB at 0.92 GHz, 1.84 GHz, 2.61 GHz, and 3.54 GHz, respectively. This research also has shown that the Figure of merit (FoM) of the proposed QB-LNA is higher than that of another multiband LNA.
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BIOGRAPHIES OF AUTHORS

Teguh Firmansyah was born in Subang, Indonesia. He received B.Eng (S.T) degree in electrical engineering and M.Eng (M.T) degree in telecommunication engineering from Department of Electrical Engineering Universitas Indonesia in 2010 and 2012, respectively. In 2012, he joined the Department of Electrical Engineering Universitas Sultan Ageng Tirtayasa as a researcher and lecturer. He has authored or coauthored over 20 papers published in refereed journals and conferences. He holds two patents for wideband antenna and multiband antenna. His research interests include microstrip antenna and microwave circuit for various applications.

Email : teguhfirmansyah@untirta.ac.id

Concurrent Quad-band Low Noise Amplifier (QB-LNA) using Multisection .... (Teguh Firmansyah)
Anggoro Suryo Pramudyo was born in 1984. He received BCS (S.Kom.) from Universitas Bina Darna in 2006 and MCS (M.Kom) from Universitas Gadjah Mada in 2006. He is interested in Artificial Intelligence included Computational Intelligence. Since 2010, he had become a lecturer and researcher at Departement of Electrical Engineering Universitas Sultan Ageng Tirtayasa. Currently his researches are about intelligent disigner for antenna. 
Email : pramudyo@untirta.ac.id

Siswo Wardoyo received the Bachelor Engineering (S.T.) in Electric Engineering from Diponegoro University of Indonesia, in 2002. Master of Engineering (M.Eng) degree, received from Electrical Engineering Department, Gadjah Mada University in 2008. Currently, he lecturer at Electrical Engineering Department, University of Sultan Ageng Tirtayasa. His research interests are My research interest are in TVET, ANN, Image Processing, Computer Vision, and Control. 
Email : siswo@untirta.ac.id

Romi Wiryadinata received the Bachelor Engineering (S.T.) in electrical engineering from Islamic University of Indonesia, in 2005. Master of Engineering (M.T.) degree, was received from Electrical Engineering Dept., Gadjah Mada University in 2007. He received Doctor (Dr.) degree from Electrical Engineering Dept., Gadjah Mada University in 2015. Currently, he is a lecturer at Electrical Engineering Dept., University of Sultan Ageng Tirtayasa. His research interests are in artificial neural network, sensor technology, guidance-control and navigation, and robotic. 
Email : wiryadinata@untirta.ac.id

Alimuddin is Associate Prof. Dr. specialization Control, Computer, Power Stability System and Energy Conversion, Telecommunication, SMART ICT and Lecture and Researcher at the Department of Electrical Engineering on Faculty of Engineering, Sultan Ageng Tirtayasa University (UNTIRTA), Banten, Indonesia, Master Engineering Informatics and Magister Information Management Graduate Binus University (BINUS) Jakarta, Master electrical engineering, Graduate Mercubuana University (UMB) Jakarta, Master computer science graduate STIMIK Nusa Mandiri Jakarta, He received B.S.and Master Management from Indonesia Moeslem University and Master Engineering for Electrical Engineering from Hasanuddin University., Indonesia in 1999, 2002 and 2003 respectively. He graduated a Doctor (PhD) Degree at the Bio-Informatics and Control, Instrumentation Engineering, Conversion Energy Bogor Agricultural University,Indonesia and Research Collaboration University of Tsukuba, Japan, 2009. Program research in Grant in sponsored by Government of Indonesia (the Ministry of Education and the State Ministry of Indonesia), He has more than 11 years of experience in teaching at several Universities. His research interests include Control System, Telecommunication, ICT, Model and Simulation, Artificial Intelligent and its application, optimization and information system, Power Stability System and Energy Conversion System, Information Technology and Computer, Distribution System, Power System Control and optimization, Transportation. He has published more than ten papers in national Journal. He has also presented more than twelve research articles in national and international conferences. He is currently with few projects sponsored by government of Indonesia (the Ministry of Education and the State Ministry). 
Email : alimudy@yahoo.com