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Design of Multi-Passband Bandpass Filters With Low-Temperature Co-Fired Ceramic Technology

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1. Introduction

Shared building blocks and power are required for the coexistence of a dual-band multimode wireless local area network and a mobile communication system. Therefore dual-passband bandpass filters have become key components at the front end of a concurrent dual-band receiver. There are several studies on dual-passband filters [1-9]. With sharper passband skirt, lower insertion loss and better selectivity may be resulted in the Zolotarev bandpass filters [1]. In [2], the dual-band filter is constructed with two parallel sets of filters. The frequency-selective resonators [3-6], stepped-impedance resonators [7, 8] and coupled resonator pairs [9] are also employed to design dual-passband filters.

In this article, we use low-temperature co-fired ceramic [10-15] technology to implement the three-dimensional (3D) multi-passband bandpass filters. Figure 1 shows the architecture of the proposed multi-passband bandpass filter, which is composed of multi-sectional short-circuit transmission lines and connected transmission lines. These transmission lines can be transferred individually to multilayered structure. Moreover, the short-circuit transmission lines may make more obvious isolation between passbands [16-18]. As a result, the proposed filter with controllable multiple passbands can be easily achieved by properly choosing the impedance and electrical length of each short-circuit transmission line and the connected transmission line.

2. Equivalent for filter synthesis

The immittance inverter [19] is adopted in this article to analyze the proposed filter. The transformed circuit of a transmission line shown in Fig. 2 can be utilized in the n-ordered multi-passband bandpass filter. Moreover, the transformed admittance inverter of the transmission line can be expressed as

\[ J_i = Y_i \csc \theta_i \]  

where \( Y_i \) and \( \theta_i \) are the corresponding admittance and electrical length of the transmission line, respectively.
By substituting the transformed transmission lines into the architecture in Fig. 1, the equivalent circuit of the proposed n-ordered multi-passband bandpass filter can be obtained as Fig. 3. The susceptance and its slope parameter are, respectively, given by

\[ B_f(f) = -\frac{1}{X_m(f)} \left( -Y_i \cot(\frac{f}{f_1}) - Y'_i \cot(\frac{f}{f_1}) \right), \quad \text{for} \quad i = 1, \ldots, n \]  

\[ b_f(f) = \frac{f}{2} \frac{\theta'_i}{f_1}, \quad \text{for} \quad i = 1, \ldots, n \quad \text{and} \quad r = 1, \ldots, m \]  

where \( f_1 \) is the central frequency of the \( r \)th passband with the corresponding fractional bandwidth \( \Delta_f \), and

\[ X_0(f) = \begin{cases} Z_m \tan(\frac{f}{f_1}), & \text{for} \quad j = 1 \\ Z_{m-1, j-1} X_{j, j-1}(f) + Z_{m-1, j} \tan(\frac{f}{f_1}), & \text{for} \quad j = 2, \ldots, m \\ Z_{m-1, j-1} - Z_{m-1, j} X_{j, j-1}(f) \tan(\frac{f}{f_1}), & \text{for} \quad j = 2, \ldots, m \end{cases} \]

Moreover, in order to match system’s impedance, 50 \( \Omega \), the input/output \( J \)-interer \( J_{0,1} \) and \( J_{0,2n+1} \) need to be set as 0.02.
Fig. 3. Equivalent circuit of the proposed n-ordered multi-passband filter

As extremely complex procedures are required for generalized formulas to synthesize the proposed multi-passband bandpass filter, only formulas for dual-passband filter synthesis are provided in detail. On the other hand, design examples of the triple- and quadruple-passband filters are offered without detailed equations.

3. Design of the dual-passband filter

To design the dual-passband filters, \( m = 2 \) should be selected. \( \Delta_1 \) and \( \Delta_2 \) are the corresponding fractional bandwidths of the first and second passband’s central frequency, \( f_1 \) and \( f_2 \), respectively. The susceptances and their slope parameters are, respectively, given by

\[
B_i(f) = Y_i \tan \left( \frac{f_1}{f} \theta_{i1} \right) \tan \left( \frac{f_2}{f} \theta_{i2} \right) - Y_i \cot \left( \frac{f_1}{f} \theta_{i1} \right) - Y_i \cot \left( \frac{f_2}{f} \theta_{i2} \right), \quad \text{for} \quad i = 1, \ldots, n
\]

\[
b_i(f) = \frac{f}{2f_i} \frac{\partial B_i(f)}{\partial f},
\]

\[
b_i(f) = \frac{f}{2f_i} \left[ \frac{Y_i \theta_{i1} \sec^2 \left( \frac{f_1}{f} \theta_i \right) \tan \left( \frac{f_2}{f} \theta_{i2} \right) \tan \left( \frac{f_1}{f} \theta_{i1} \right) + Y_i \tan \left( \frac{f_2}{f} \theta_{i2} \right) \tan \left( \frac{f_1}{f} \theta_{i1} \right)}{Y_i \tan \left( \frac{f_1}{f_i} \theta_{i1} \right) + Y_i \tan \left( \frac{f_2}{f_i} \theta_{i2} \right)} + \frac{Y_i \theta_{i1} \sec^2 \left( \frac{f_2}{f} \theta_i \right) \tan \left( \frac{f_1}{f} \theta_{i2} \right) \tan \left( \frac{f_2}{f} \theta_{i1} \right) + Y_i \tan \left( \frac{f_1}{f} \theta_{i2} \right) \tan \left( \frac{f_2}{f} \theta_{i1} \right)}{Y_i \tan \left( \frac{f_1}{f} \theta_{i2} \right) + Y_i \tan \left( \frac{f_2}{f} \theta_{i1} \right)} \right], \quad \text{for} \quad i = 1, \ldots, n \quad \text{and} \quad r = 1 \text{ or } 2
\]
where \( Y_0 = Y_n = 0 \).

Consequently, we can obtain the following equations

\[
J_{i+1} = \Delta J_i \frac{h_i^2}{g_i g_{i+1}} = \Delta J_i \frac{h_i^2}{g_i g_{i+1}}, \quad \text{for } i = 1, \ldots, n-1
\]

(7)

\[
\Delta J_i = \Delta J_{i+1}
\]

(8)

where \( g_i \)'s are the element values of the prototypical lowpass filter.

The procedures of developing the bandpass filter with controllable dual passbands are provided below.

### 3.1 Formula development

#### A. Equal bandwidth \((\Delta_1 f_1 = \Delta_2 f_2)\)

With \( \theta_1 = \theta_2 = \theta_0 = \theta_0 \) and \( R_i \) as the ratio of \( f_i \) to \( f_0 \), the following equations are derived

\[
b_i = R_i b_0
\]

(9)

\[
\sec(\theta_0) = -\sec(R_i \theta_0)
\]

(10)

\[
Y_i = \frac{g_o s_i}{R_i \sqrt{g_i g_{i+1}}} \sin \theta_0
\]

(11)

\[
Y_i = \frac{g_o s_i}{R_i \Delta_i \theta_0} - Y_0
\]

(12)

\[
Y_i = Y_i + \tan^2 \theta_0 \frac{R_i \Delta_i \theta_0 Y_i \sec^2 \theta_0}{g_o s_i}
\]

(13)

\[
Y_i = Y_{i+1} + Y_i
\]

(14)

As the fractional bandwidth of the passband is characterized by the 3 dB band-edge frequency of lower and upper bands, a steeper slope and a narrower bandwidth in the passband may be obtained with an increasing order of the filter. As a result, the formula of \( \Delta_i \) needs to be modified. With the assistance of statistical inferences, the orders, \( \Delta_1 \) and \( R_i \) of the proposed dual-passband filter should be in the range of 3-8, 1-21% and 1.5-4, respectively. Therefore the modified formula can be expressed as

\[
\Delta_{in} = MF_{in} + MF_{ni}
\]

(15)

\[
MF_{in} = 0.9 + (R_i - 1.5) \left[ 0.5 + 0.2(N - 3) \right] + \sum_{i=1}^{N} \left[ 0.25 + 0.08(i - 4) \right]
\]

(16)

\[
MF_{ni} = \begin{cases} (\Delta_i - 1) \left[ MF + 0.01 (N - 1) \right], & 1 \% \leq \Delta_i \leq 14 \% \\ (\Delta_i - 1)MF, & \Delta_i = 21 \% \\ 0.76, & N = 3 \text{ and } R_i = 1.5 \\ 0.76 [1.29 + A(N - 4)], & N \geq 4 \text{ and } R_i = 1.5 \\ 0.76 [1.29 + A(N - 4)] [1.31 + 0.75(R_i - 2)], & N \geq 4 \text{ and } R_i > 1.5 \end{cases}
\]

(17)

(18)
Consequently provided below.

### A. Equal bandwidth \((\Delta_1 f_1 = \Delta_2 f_2)\)

When the bandwidths of two passbands are unequal, the electrical lengths, \(\theta_1\) and \(\theta_2\), are not equal, either. With \(\theta_1 = \theta_b\) and \(\theta_2 = \theta_{b1} = \theta = \theta_n\), the following equations are obtained

\[
\begin{align*}
A &= \begin{cases} 
0.18, & 3 \leq N \leq 5 \\
0.12, & 6 \leq N \leq 8
\end{cases} \quad (19)
\end{align*}
\]

### B. Unequal bandwidth \((\Delta_1 \neq \Delta_2)\)

When the bandwidths of two passbands are unequal, the electrical lengths, \(\theta_1\) and \(\theta_2\), are not equal, either. With \(\theta_1 = \theta_b\) and \(\theta_2 = \theta_{b1} = \theta = \theta_n\), the following equations are obtained

\[
\begin{align*}
B &= \left[ \cot \theta_1 \sec^2 \theta_1 + \cot \theta_2 \sec^2 \theta_2 \right] + \csc^2 \theta_1 + \csc^2 \theta_2 \tan \theta_1 \tan \theta_2 - \cot(R \theta_1 \theta_2) \tan(R \theta_1 \theta_2) \\
C &= \tan \theta_1 \sec \theta_1 - \tan(R \theta_1 \theta_2) \tan(R \theta_1 \theta_2) \left[ \tan \theta_2 + \cot \theta_2 \right] \\
D &= \tan(R \theta_1 \theta_2) \sec^2(R \theta_1 \theta_2) \left[ \cot \theta_2 \tan(R \theta_1 \theta_2) - \cot(R \theta_1 \theta_2) \tan(R \theta_1 \theta_2) \right] \tan \theta_1 \tan \theta_2 - \tan(R \theta_1 \theta_2) \tan(R \theta_1 \theta_2) \\
E &= \tan(R \theta_1 \theta_2) - \tan \theta_1 \tan \theta_2 - \tan \theta_1 \tan \theta_2 \left[ \tan \theta_2 + \cot \theta_2 \right] \\
G &= Y_1^2 \left( \csc^2 \theta_1 + \cot \theta_1 \csc^2 \theta_1 \right) \tan \theta_1 \tan \theta_2 - \cot \theta_1 \csc^2 \theta_1 \tan \theta_1 \tan \theta_2 \\
H &= 2Y_1^2 \tan \theta_1 \tan \theta_2 \\
K &= 2\left[ \csc^2 \theta_1 + \cot \theta_1 \csc^2 \theta_1 - \cot \theta_2 \csc^2 \theta_2 \right] + \csc^2 \theta_2 \tan \theta_1 \tan \theta_2 \\
P &= \left[ \csc^2 \theta_2 \tan \theta_1 \tan \theta_2 + \cot \theta_2 \csc^2 \theta_2 + \cot \theta_2 \csc^2 \theta_2 \tan \theta_1 \tan \theta_2 \right] - \left[ \csc^2 \theta_2 \tan \theta_1 \tan \theta_2 + \cot \theta_2 \csc^2 \theta_2 \tan \theta_1 \tan \theta_2 \right] \\
Q &= \left[ \csc^2 \theta_2 \tan \theta_1 \tan \theta_2 + \cot \theta_2 \csc^2 \theta_2 + \csc^2 \theta_2 \tan \theta_1 \tan \theta_2 \right] - \left[ \cot \theta_2 \csc^2 \theta_2 \tan \theta_1 \tan \theta_2 \right] \\
S &= \cot \theta_2 \left( \csc^2 \theta_2 \tan \theta_1 \tan \theta_2 - \cot \theta_2 \csc^2 \theta_2 \tan \theta_1 \tan \theta_2 \right) \\
\end{align*}
\]

Similarly, the orders, \(\Delta_1\) and \(R_f\) of the proposed dual-passband filter should be in the range of 3-6, 2-15% and 2.17-3.5, respectively. Therefore the formula of \(\Delta_1\) needs to be modified as

\[
\Delta_{in} = (M_{F_1} + M_{F_2}) \cdot \Delta_1 \quad (34)
\]

where

\[
M_{F_1} = 1.38 - 0.031(\Delta_1 - 4) + 0.29(\Delta_1 - 3) \quad (35)
\]

\[
M_{F_2} = 2(R_f - 2.17)(0.58 - 0.033(\Delta_1 - 4)) \quad (36)
\]
3.2 Simulation and Experimental Results

Following are design examples of the three-ordered dual-passband bandpass filters with multilayered structure. Below are fabricated examples categorized by two passbands with equal or unequal bandwidths.

A. Two passbands with equal bandwidth \((\Delta f_1 = \Delta f_2)\)

Figure 4 shows the three-ordered dual-passband filter. The central frequencies of two passbands are set at 2 and 5.3 GHz. The bandwidth of both passbands is chosen as 260 MHz, which is 13% of the first passband’s central frequency. Moreover, the selected ripple for the prototypical Chebyshev lowpass filter is 0.01 dB. As a result, the electrical length \(\theta_0\) and the impedances \(Z_{11}, Z_{12}, Z_{21}, Z_{22}\) and \(Z_1\) are obtained as 49.3°, 14.59, 14.64, 17.75, 27.71 and 81.9 \(\Omega\), respectively. According to these calculated parameters, theoretical predictions of the dual-passband bandpass filter are shown in Fig. 5c. Furthermore, with the assistance of full-wave electromagnetic simulator—Sonnet (Sonnet Software Inc.), these calculated parameters are converted into the multilayered structure.

![Figure 4. Architecture of the three-ordered dual-passband filter whose passbands have equal bandwidth](image)

The proposed multilayered dual-passband bandpass filter is fabricated on Dupont 951, whose dielectric constant and loss tangent are 7.8 and 0.0045, respectively. The multilayered 2/5.3 GHz bandpass filter is designed on 11 substrates of 0.09 mm, and its overall size is 4.98 mm \(\times\) 4.01 mm \(\times\) 0.99 mm. Figures 5a and 5b show the 3D architecture and the photograph of this fabricated filter; Fig. 5c also presents the measured results.
3.2 Simulation and Experimental Results

Following are design examples of the three-ordered dual-passband bandpass filters with multilayered structure. Below are fabricated examples categorized by two passbands with equal or unequal bandwidths.

**A. Two passbands with equal bandwidth ($\Delta f_1 = \Delta f_2$)**

![3D architecture](image1)

Figure 4 shows the three-ordered dual-passband filter. The central frequencies of two passbands are set at 2 and 5.3 GHz. The bandwidth of both passbands is chosen as 260 MHz, which is 13% of the first passband’s central frequency. Moreover, the selected ripple for the prototypical Chebyshev lowpass filter is 0.01 dB. As a result, the electrical length $\theta_0$ and the impedances $Z_{11}$, $Z_{12}$, $Z_{21}$, $Z_{22}$, and $Z_1$ are obtained as 49.3°, 14.59, 14.64, 17.75, 27.71, and 81.9 $\Omega$, respectively. According to these calculated parameters, theoretical predictions of the dual-passband bandpass filter are shown in Fig. 5. Furthermore, with the assistance of full-wave electromagnetic simulator – Sonnet (Sonnet Software Inc.), these calculated parameters are converted into the multilayered structure.

![Photograph](image2)

Fig. 4. Architecture of the three-ordered dual-passband filter whose passbands have equal bandwidth

The proposed multilayered dual-passband bandpass filter is fabricated on Dupont 951, whose dielectric constant and loss tangent are 7.8 and 0.0045, respectively. The multilayered 2/5.3 GHz bandpass filter is designed on 11 substrates of 0.09 mm, and its overall size is 4.98 mm $\times$ 4.01 mm $\times$ 0.99 mm. Figures 5a and 5b show the 3D architecture and the photograph of this fabricated filter; Fig. 5c also presents the measured results.

![Diagram](image3)

(c) Responses of the theoretical prediction and measurement

Fig. 5. Three-ordered 2/5.3 GHz dual-passband bandpass filter whose passbands have equal bandwidth

On the one hand, within the first passband (1.8-2.2 GHz), the measured insertion loss is < 1.6 dB, whereas the return loss is > 18 dB. On the other hand, within the second passband (5.16-5.51 GHz), the measured insertion loss is < 2.2 dB, whereas the return loss is also > 18 dB.

**B. First passband with greater bandwidth ($\Delta f_1 > \Delta f_2$)**

![Diagram](image4)

Figure 6 shows the architecture of the three-ordered dual-passband filter. The central frequencies of two passbands are set at 2 and 5.3 GHz. The bandwidths of the first and second passband are chosen as 300 and 200 MHz, respectively, which are 15% and 10% of the first passband’s central frequency. Moreover, the selected ripple for the prototypical
Chebyshev lowpass filter is 0.01 dB. With the electrical length $\theta_a$ as 35.9°, the electrical length $\theta_b$ and the impedances $Z_{11}$, $Z_{12}$, $Z_{21}$, $Z_{22}$ and $Z_1$ are then obtained as 64.3°, 14.17, 13.44, 18.64, 28.34 and 88.24 $\Omega$, respectively. According to these calculated parameters, theoretical predictions of the dual-passband bandpass filter are shown in Fig. 7c.

The multilayered 2/5.3 GHz bandpass filter is fabricated on 12 substrates of 0.09 mm, and its overall size is 4.98 mm $\times$ 4.06 mm $\times$ 1.08 mm. Figures 7a and 7b show the 3D architecture and the photograph of this fabricated filter; Fig. 7c also presents the measured results.
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On the one hand, within the first passband (1.79-2.35 GHz), the measured insertion loss is < 1.6 dB, whereas the return loss is > 20 dB. On the other hand, within the second passband (5.2-5.5 GHz), the measured insertion loss is < 2.1 dB, whereas the return loss is > 15 dB.

C. First passband with smaller bandwidth ($\Delta f_1 < \Delta f_2$)

Figure 6 also shows the architecture of the three-ordered dual-passband filter. The central frequencies of two passbands remain as 2 and 5.3 GHz. The bandwidths of the first and second passband are chosen as 200 and 300 MHz, respectively, which are 10% and 15% of first passband’s central frequency. Moreover, the selected ripple for the prototypical Chebyshev lowpass filter is 0.01 dB. With the electrical length $\theta_a$ as 51°, the electrical length

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(c) Responses of the theoretical prediction and measurement

Fig. 7. Three-ordered 2/5.3 GHz dual-passband bandpass filter whose first passband’s bandwidth is greater

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(a) 3D architecture                                         (b) Photograph

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Fig. 8. Three-ordered 2/5.3 GHz dual-passband bandpass filter whose first passband's bandwidth is smaller

The impedances $Z_{11}$, $Z_{12}$, $Z_{21}$, $Z_{22}$ and $Z_1$ are then obtained as 47.1°, 11.89, 11.2, 11.28, 13.69 and 74.59 Ω, respectively. According to these calculated parameters, theoretical predictions of the dual-passband bandpass filter are shown in Fig. 8c.

The multilayered 2/5.3 GHz bandpass filter is fabricated on 10 substrates of 0.09 mm, and its overall size is 4.98 mm $\times$ 3.6 mm $\times$ 0.9 mm. Figures 8a and 8b show the 3D architecture and the photograph of this fabricated filter; Fig. 8c also presents the measured results.

On the one hand, within the first passband (1.85-2.22 GHz), the measured insertion loss is < 1.8 dB, whereas the return loss is > 20 dB. On the other hand, within the second passband (5.14-5.62 GHz), the measured insertion loss is < 2.5 dB, whereas the return loss is > 18 dB.

4. Multi-passband filter fabrication

The multi-passband filter can be obtained from (1) to (4). The fabricated examples of triple- and quadruple-passband filters are introduced below.

4.1 Triple-passband filter

Figure 9 shows the architecture of the three-ordered triple-passband filter. The central frequencies of three passbands are set as 2, 5 and 8 GHz. The bandwidths of the first, second and third passband are chosen as 200, 300 and 200 MHz, respectively, which are 10%, 15% and 10% of the first passband’s central frequency. Moreover, the selected ripple for the prototypical Chebyshev lowpass filter is 0.01 dB. With the electrical length $\theta_e$ as 35.5°, the electrical length $\theta_b$ and the impedances $Z_{11}$, $Z_{12}$, $Z_{13}$, $Z_{21}$, $Z_{22}$, $Z_{23}$ and $Z_1$ are then obtained as 37.2°, 20.3, 17.51, 20.34, 29.89, 13.21, 29.84 and 67.7 Ω, respectively. According to these calculated parameters, theoretical predictions of the triple-passband bandpass filter are shown in Fig. 10c.
Fig. 9. Architecture of the three-ordered triple-passband filter whose passbands have unequal bandwidths.

The multilayered 2/5/8 GHz bandpass filter is fabricated on 10 substrates of 0.09 mm, and its overall size is 4.72 mm × 3.7 mm × 0.9 mm. Figures 10a and 10b show the 3D architecture and the photograph of this fabricated filter; Fig. 10c also presents the measured results.
Within the first passband (1.66-2.11 GHz), the measured insertion loss is < 1.4 dB, whereas the return loss is > 16.8 dB. Moreover, within the second passband (4.6-5.35 GHz), the measured insertion loss is < 1.8 dB, whereas the return loss is > 16 dB. Furthermore, within the third passband (7.84-8.14 GHz), the measured insertion loss is < 3 dB, whereas the return loss is > 15 dB.

4.2 Quadruple-passband filter

Figure 11 shows the architecture of the three-ordered quadruple-passband filter. The central frequencies of four passbands are set as 2, 5, 8 and 11.3 GHz. The bandwidth of four passbands is all chosen as 180 MHz, which is 9% of the first passband’s central frequency. Moreover, the selected ripple for the prototypical Chebyshev lowpass filter is 0.01 dB. As a result, the electrical length $\theta_0$ and the impedances $Z_{11}, Z_{12}, Z_{13}, Z_{14}, Z_{21}, Z_{22}, Z_{23}, Z_{24}$ and $Z_1$ are obtained as 26.8°, 21.79, 19.61, 22.74, 14.54, 27.49, 16.01, 14.04, 19.84 and 71.5 $\Omega$, respectively. According to these calculated parameters, theoretical predictions of the quadruple-passband bandpass filter are shown in Fig. 12c.
Fig. 11. Architecture of the three-ordered quadruple-passband filter whose passbands have equal bandwidth
The multilayered 2/5/8/11.3 GHz bandpass filter is fabricated on 12 substrates of 0.09 mm, and its overall size is 4.72 mm × 3.7 mm × 1.08 mm. Figures 12a and 12b show the 3D architecture and the photograph of this fabricated filter; Fig. 12c also presents the measured results. Within the first passband (1.77-2.3 GHz), the measured insertion loss is < 1 dB, whereas the return loss is > 17 dB. Moreover, within the second passband (5.14-5.48 GHz), the measured insertion loss is < 1.8 dB, whereas the return loss is > 16 dB. In addition, within the third passband (8.06-8.4 GHz), the measured insertion loss is < 3 dB, whereas the return loss is > 15 dB. Furthermore, within the fourth passband (11.05-11.85 GHz), the measured insertion loss is < 4 dB, whereas the return loss is > 12.5 dB.

5. Conclusion

A novel structure of the multi-passband bandpass filters has been proposed in this article. Multi-sectional short-circuit transmission lines shunted with transmission lines are utilized. By properly choosing the proposed structure’s electrical lengths and impedances, multiple passbands can be easily controlled.

In addition, the design procedures have been described in detail, and 3D architectures are provided. Because of the parasitic effect among capacitors for a physical 3D circuit, there is some slight difference between the theoretical predictions and measured results. However, generally speaking, the measured results match well with the theoretical predictions. Therefore with high integration and compact size, the proposed multi-passband filter is suitable for implementation in a multi-chip module.

By the way, because insertion loss measurement is related to the degree and bandwidth of a filter, the performance of a filter with resonators can be well indicated by translating the measurement into an unloaded Q of a resonator.
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6. References

[1] Bell, H. C. (2001). Zolotarev bandpass filters, IEEE Trans. Microw. Theory Tech., Vol. 49, No. 12, pp. 2357-2362
[2] Miyake, H.; Kitazawa, S.; Ishizaki, T.; Yamada, T. & Nagatomi, Y. (1997). A miniaturized monolithic dual band filter using ceramic lamination technique for dual mode portable telephones, Proceedings of IEEE MTT-S Int. Microw. Symp. Dig., pp. 789-792
[3] Quendo, C., Rius, E. & Person, C. (2003). An original topology of dual-band filter with transmission zeros, Proceedings of IEEE MTT-S Int. Microw. Symp. Dig., pp. 1093-1096
[4] Chang, C. H.; Wu, H. S.; Yang, H. J. & Tzuan, C. K. C. (2003). Coalesced single-input single-output dual-band filter, Proceedings of IEEE MTT-S Int. Microw. Symp. Dig., pp. 511-514
[5] Tsai, C. M.; Lee, H. M. & Tsai, C. C. (2005). Planar filter design with fully controllable second passband, IEEE Trans. Microw. Theory Tech., Vol. 53, No. 11, pp. 3429-3439
[6] Yim, H. Y. & Cheng, K. K. M. (2005). Novel dual-band planar resonator and admittance inverter for filter design and applications, Proceedings of IEEE MTT-S Int. Microw. Symp. Dig., pp. 2187-2190
[7] Lee, J.; Uhm, M. S. & Yom, I. B. (2004). A dual-passband filter of canonical structure for satellite applications, IEEE Microw. Wireless Comp. Lett., Vol. 14, No. 6, pp. 271-273
[8] Kuo, J. T.; Yeh, T. H. & Yeh, C. C. (2005). Design of microstrip bandpass filters with a dual-passband response, IEEE Trans. Microw. Theory Tech., Vol. 53, No. 4, pp. 1331-1337
[9] Chen, C. C. (2005). Dual-band bandpass filter using coupled resonator pairs, IEEE Microw. Wireless Comp. Lett., Vol. 15, No. 4, pp. 259-261
[10] Rong, Y.; Zaki, K. A.; Hageman, M.; Stevens, D. & Gipprich, J. (1999). Low temperature cofired ceramic (LTCC) ridge waveguide bandpass filters, Proceedings of IEEE MTT-S Int. Microw. Symp. Dig., pp. 1147-1150
[11] Heo, D.; Sutono, A.; Chen, E.; Suh, Y. & Laskar, J. (2001). A 1.9 GHz DECT CMOS power amplifier with fully integrated multilayer LTCC passives, IEEE Microw. Wireless Comp. Lett., Vol. 11, No. 6, pp. 249-251
[12] Leung, W. Y.; Cheng, K. K. M. & Wu, K. L. (2001). Design and implementation of LTCC filters with enhanced stop-band characteristics for bluetooth applications, Proceedings of Asia-Pacific Microw. Conf., pp. 1008-1011
[13] Tang, C. W.; Sheen, J. W. & Chang, C. Y. (2001). Chip-type LTCC-MLC baluns using the stepped impedance method, IEEE Trans. Microw. Theory Tech., Vol. 49, No. 12, pp. 2342-2349
[14] Tang, C. W.; Lin, Y. C. & Chang, C. Y. (2003). Realization of transmission zeros in combine filters using an auxiliary inductively-coupled ground plane, IEEE Trans. Microw. Theory Tech., Vol. 51, No. 10, pp. 2112-2118
[15] Tang, C. W. (2004). Harmonic-suppression LTCC filter with the step impedance quarter-wavelength open stub, IEEE Trans. Microw. Theory Tech., Vol. 52, No. 2, pp. 617-624
[16] Tang, C. W.; You, S. F. & Liu, I. C. (2006). Design of a dual-band bandpass filter with low temperature co-fired ceramic technology, IEEE Trans. Microw. Theory Tech., Vol. 54, No. 8, pp. 3327-3332

www.intechopen.com
[17] Sun, S. & Zhu, L. (2006). Novel design of microstrip bandpass filters with a controllable dual-passband response: description and implementation, *IEICE Trans. Electron.*, Vol. E89-C, No. 2, pp.197-202

[18] Quendo, C.; Manchec, A.; Clavet, Y.; Rius, E.; Favennec, J. F. & Person, C. (2007). General Synthesis of N-Band Resonator Based on N-Order Dual Behavior Resonator, *IEEE Microw. Wireless Comp. Lett.*, Vol. 17, No. 5, pp. 337-339

[19] Matthaei, G.L.; Young, L. & Jones, E.M. (1980). *Microwave filters, impedance-matching network, and coupling structures*, Artech House, Norwood, MA
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