Comparative analysis of sokal’s equations versus load-pull implementation of class E low-pass network

B. Kirish¹, F. Zubir², M. K. A. Rahim³, S. M. Shah⁴

¹,²Communication Engineering Department, Universiti Teknologi Malaysia, Malaysia
³School of Engineering, University of British Columbia, Canada
⁴Department of Communication Engineering, Universiti Tun Hussein Onn Malaysia (UTHM), Malaysia

ABSTRACT

In this paper, Class E power amplifiers (PA) aimed at frequency bandwidth of 3.4 GHz to 3.6 GHz (LTE 42) and 3.6 GHz to 3.8 GHz (LTE 43) respectively are designed with objective of attaining high efficiency. The viability of Sokal’s equations for present communication systems aimed at GHz are analyzed for high efficiency using HEMT (High-electron-mobility transistor) on Nitronex NPTB00004 as opposed to the Bipolar Junction Transistor used by Sokal in 1975. Load-pull configuration techniques aimed at the drain is implemented at the output matching network (OMN) and benchmarked against Sokal’s equation. At the OMN, to suppress harmonics, band-pass filters are employed for the LTE 42 and 43 respectively. Sokal’s equation shows that the drain must be conjugately matched before his equations are applied at the OMN. The efficiency at 3.4 GHz obtained for Sokal’s circuit is at 67 % and gain of 9.3 dB. More than 65% efficiency is obtained from load-pull network at 3.4 GHz to 3.76 GHz before filter implementation while showing gain above 7.8 dB. After filter addition at OMN, the efficiency is above 65% and gain above 8 dB for dual-band having bandwidth of 3.4389 GHz - 3.542GHz and 3.6569GHz - 3.8GHz.

Keywords: Bandpass filter, Class E PA, GaN, Harmonic termination, Low-pass matching network

Corresponding Author:
Boodhoo Kirish,
Communication Engineering Department,
Universiti Teknologi Malaysia, 81310 Johor Bahru, Malaysia.
Email: boodhookirish@gmail.com

1. INTRODUCTION

The present era has shown that highly efficient power amplifiers (PA) are a necessity for newly advanced wireless communication systems [1-3] in terms of achieving a low cost as well as reliable transmitters [4, 5]. A PA can be defined as an amplifier designed whereby the maximum power is transferred only for a selection of active devices such as transistors [6]. There are numerous advantages for circuits and systems involving RF and microwave sector in terms of power amplification methods which aims for high efficiency. In the RF and microwave engineering, it is a well-founded knowledge that high efficiency power amplifiers greatly improves the power consumption of a communication system as well as reduces the size and weight of radio transmitters. One of the main problems in techniques involving amplification, it is very difficult to use high efficiency power amplification techniques for operations involving high frequencies and high power level as the capacitance of devices used will cause hindrance in achieving desired result i.e. high efficiency and gain. Therefore the role of class of PA comes in the picture and designers use different classes of PA to solve different problems [7-9]. An example of power amplifier that enables high efficiency is Class E [5, 10-12] due to its ability of being unaffected to the transistor switching problems such as power losses in the transistor and capacitances of the transistor affecting the output [7, 13-16]. Theoretically Class E PAs can attain 100% efficiency [1, 17].
In [18] the switching operation works the same as normal Class E amplifier would work and therefore attain the theoretical 100% efficiency. It employs two parallel resonators and a decoupling capacitor so as to reject the second harmonic (HD2) emission shown in while also providing a DC path for the supply current. The impedance-transformation technique in [19] for Class E PA to improve the reactance-compensation network whereby without adding any more components, the desired load resistance can be four times the original value, while the flat load angle is sustained. This means the output matching network at the drain can be significantly simplified. Therefore by implementing the exact number of components in the matching network, a greater operational bandwidth can be achieved and the extra network to match the output load is therefore made redundant. The method employed in [20] is such that the current fall time of switch is considerably reduced all while keeping the operating frequency to be quite large so that it will be possible to ignore the switching time of the transistor. The bi-harmonic operation (that is second harmonic) is considered as it is the largest harmonic and has to be eliminated. Trying to solve all multi-harmonic mode imposes considerable complications due to circuit complexity, while does not seem to offer any advantage as the power of the other harmonics are too low. The second harmonic frequency is tackled by harmonic injection method. The work [21] states that for the Class-E PA input and output matching networks design should aim to provide optimum impedances for both gate and drain connections of the active device in the required frequency. The broadband class-E power amplifier for 1.8 GHz–2.7 GHz LTE frequency range has to employ load/source–pull measurement for the range of frequencies to obtain accurate optimum load and source impedances of the active device. The use of Sokal’s equation has been used to calculate the OMN matching network after which the lumped components have been converted to microstrip lines as the author claims that it is the impedance matching at the drain that will achieve Class E operation. The work was aimed at dual band operation and based on Sokal’s equations would give two sets of lumped components. However by making use of transmission lines that satisfy the requirements of both lumped components the circuit can be transformed to microstrip lines [22]. In the work [23] Class E operation was performed only at simulation level using Sokal’s equations however it does provide a useful insight on how the implementation of Sokal’s formula at different transistors affect the power added efficiency (PAE). Although no fabrication was done, the Class E implementation on three different transistors has shown different efficiency and output power despite being matched by the same OMN that is based on Sokal’s equations. Nevertheless the insight provided in this paper has allowed the research done within this paper to prove that the impedance at the drain need to be addressed first before implementing Sokal’s formulas and that not all transistors will be able to achieve same efficiency at same frequency despite same OMN.

2. RESEARCH METHOD

2.1. Stability of transistor

The stability of a transistor is a primordial factor that has to be taken into consideration when designing a power amplifier. Usually the design of an amplifier involves the use of stability circles whereby if the $|S_{11}|$ of the transistor is less than 1 then the stable region should be located outside the stability circles while if the opposite is true then the stable region is found inside [24]. However, such a concept cannot be applied here as the stability region would always change when the frequency of operation is changed. Hence if we are designing an amplifier for a wide range of frequencies such as multiband concept then it may happen that for some frequencies it will be stable while for others it will not work as amplifier. Therefore, we would need to choose a transistor that can be implemented over a wide range of frequencies where it is unconditionally stable. This is usually tested by employing the Rollet’s condition as shown in (1) and (2) [3, 24-27].

\[
K = \frac{1+|A|^2-|S_{11}|^2-|S_{22}|^2}{2|S_{12}S_{21}|} > 1
\]

\[
|A| = S_{11} S_{22} - S_{12} S_{21} < 1
\]

It is shown in Figure 1(a) that the transistor is unconditionally stable for a wide range of frequencies from DC up till 6 GHz. Although it is able to operate beyond that but for efficiency reasons, we choose not to implement it above this range. The next step is to test whether the transistor is able to work as an amplifier or not which is shown in Figure 1(b) that the transistor can work as amplifier. It is to be noted thought that there is indeed a correlation between the gain and stability of the amplifier as from Figure 1(a) that the transistor is very stable at lower frequencies and also in Figure 1(b) the transistor shows higher gain at lower frequencies.

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2.2. Class E PA using Sokal’s equations

It is already known that Class E works as a switching mode amplifier and was invented in 1970s by Nathan Sokal and Alan Sokal [28]. The basic topology of the Class-E PA is shown in Figure 2.

![Figure 2. Basic Class E amplifier schematic [6]](image)

Using Sokal’s equations presented in [29] as shown in (3) – (6) below. These components are calculated based on specific supply voltage $V_{DC}$ and required output power $P_{OUT}$. The Loaded quality factor ($Q_L$) is a free choice variable where the most suitable range for an efficiency and linearity that is applicable for design is usually chosen between 5 and 10. The $Q_L$ values are chosen by designers with the knowledge that there will be a trade-off between frequency of operation and elimination of harmonics. The equations provided by Sokal’s are derived with the duty ratio set at the usual choice that is 50% as stated in [29] and the minimum value of $Q_L$ is 1.7879 [28].

$$R_{LOAD} = 0.5786 \left( \frac{V_{DD}}{P_{out}} \right) \left( 1 - \frac{0.451759}{Q_L} - \frac{0.402444}{Q_L^2} \right)$$  \hspace{1cm} (3)

$$C_s = \frac{1}{\omega R_L} \left( \frac{1}{Q_L - 0.104823} \left( 1 + \frac{1.101468}{Q_L - 1.7879} \right) \frac{0.2}{\omega^2 L_s} \right)$$  \hspace{1cm} (4)

$$C_p = \frac{1}{5.44668 \omega R_L} \left( 1 + \frac{0.91424}{Q_L} - \frac{1.03175}{Q_L^2} \right) + \frac{0.6}{\omega^2 L_s}$$  \hspace{1cm} (5)

$$L_s = \frac{Q_L R_L}{\omega}$$  \hspace{1cm} (6)
These equations give the values of the passive components for the output matching network (OMN) design which will enable a non-overlapping current voltage waveform which is primordial for achieving a very high efficiency. The loaded quality factor $Q_L$ plays a vital role in the design of the amplifier as the output will change depending on the value that has been assigned to $Q_L$. The Table 1 display the values obtained from the (3) to (6) in order to calculate the output matching network parameters. It is important to know that $V_{gs}$ is constantly maintained at a DC bias of -2.0 V at pinch-off condition while $V_{ds} = 10$ V. The circuit of the Class E PA based on Sokal’s equation is shown in Figure 3. The load-pull will give us the maximum gain and efficiency that can be achieved by the transistor at 3.4 GHz. From that reflection coefficient obtained we can thus build our required circuit. The load-pull output shown in Figure 4 shows at which point we can obtain the best results for both power added efficiency and output power.

| Passive Component (OMN) | Values ($Q_L = 10$, $F = 3.4$GHz) |
|-------------------------|-----------------------------------|
| $R_L$                   | 50Ω                               |
| $C_P$                   | 0.242pF                           |
| $C_S$                   | 0.089pF                           |
| $L_s$                   | 23.41nH                           |

Table 1. Values for the passive component in Class E OMN

Figure 3. Sokal’s Class E circuit implemented with S22 matching of the transistor

Figure 4. Load –Pull contour lines showing results for 3.4 GHz

2.3. Dual-band class E PA

The lumped elements were transformed from the impedances obtained from the load pull and the conjugate matching. The main concept in converting the reflection coefficient here to lumped components is by taking the load-pull reflection coefficient as a conjugate value and then matching it to create the same reflection coefficient at the drain. The same technique is applied for the reflection coefficient of $S_{11}$ at the gate. The circuit is shown in Figure 5 which display the NPTB0004 transistor connected with the translated reflection coefficient to lumped components at both input and output.
Figure 5. Implementation of Class E power amplifier based on lumped components

Usually harmonics in Class E is terminated by using open circuit stubs aimed at each harmonics frequencies [6]. But since in this project the aim is for the Class E operation at dual band then matching each specific harmonics is not a viable option which is why band pass filter is implemented and designed by using the (7) to (13) from Pozar [24]. Since LTE band 42 and 43 is the main bandwidth frequency therefore it is preferred to implement a bandpass filter to have cut-off frequencies of 3.35GHz to 3.85 GHz. The center frequency can be calculated by the (7) stated below which is obtained at 3.59 GHz.

\[
\omega_c = \sqrt{\frac{F_1 \times F_2}{F_2}}
\]

(7)

\[
\Delta = \frac{F_2 - F_1}{\sqrt{F_1 F_2}}
\]

(8)

\[
\frac{\omega}{\omega_c} = \frac{1}{\Delta} \left( \frac{\omega}{\omega_c} - \frac{\omega_c}{\omega} \right)
\]

(9)

\[
L'_1, L'_2 = \frac{g_K R_0}{\omega_0 \Delta}
\]

(10)

\[
C'_1, C'_2 = \frac{\Delta}{\omega_0 g_K R_0}
\]

(11)

\[
L'_2 = \frac{\Delta R_0}{\omega_0 g_K}
\]

(12)

\[
C'_2 = \frac{g_K}{\omega_0 \Delta R_0}
\]

(13)

The order of the filter is very important as it tell us how many components are going to be incorporated and secondly how steep the response is going to be. Based on the attenuation versus normalized frequency and element values for maximally low pass filter values taken from [24]. Then based on the order, the element values from Table 2 can be obtained which will be used to calculate the capacitors and inductors for the band-pass filter.

Finally, the design bandpass filter is shown in Figure 6(a) by using the calculated values of capacitors and inductors. To prove that the filter is indeed working a simple frequency response curve of S₁₁ and S₂₁ against frequency in Figure 6(b) clearly shows that the filter works as it filters out all frequencies before 3.35 GHz and after 3.85 GHz thereby allowing the main frequencies of LTE 42 and 43 to pass through. The filter is then added to the main Class E power amplifier shown in Figure 5 where then the newly formed power amplifier incorporated with harmonic filter is shown in Figure 7.
Table 2. Band-pass filter Parameters for (\(g_1, g_2 = 1.0, g_3 = 2.0\), \(\omega_0 = 2\pi \times 3.59\) GHz, \(\Delta = 0.139, R_0 = 50\ \Omega\).)

| Element | Values   |
|---------|----------|
| \(L_1\), \(L_1\) | 15.8765 nH |
| \(C_1\), \(C_1\) | 0.12311 pF |
| \(L_2\) | 0.1538 nH |
| \(C_2\) | 12.701 pF |

Figure 6. (a) Band pass filter for elimination of harmonics (b) \(S_{11}\) and \(S_{21}\) parameters of the band-pass filter.

Figure 7. Class E power amplifier with bandpass filter for harmonics terminations.

3. RESULTS AND DISCUSSION

In this section, it is explained the results of research and at the same time is given the comprehensive discussion. Results can be presented in figures, graphs, tables and others that make the reader understand easily [2, 5]. The discussion can be made in several sub-chapters.

3.1. Sokal’s class E results

The use of Sokal’s formula to the design of Class E amplifier was a bit tricky. Sokal’s equations were derived more than 3 decades ago and technology at that time were not as advanced as todays. The results shown in Figure 8 displays very poor efficiency and relatively narrow bandwidth. Hence if we wanted to prove the operation ability of Sokal’s equation and why in this case it is now working, a new design has to be added to this present output matching network.

Sokal’s equation did not account for the reflection coefficient needed at the drain of the transistor to satisfy the efficient way of transferring power. Hence at this point, \(S_{22}\) conjugate matching has been employed and the relevant impedance obtained from the \(S_{22}\) conjugate reflection coefficient has been converted to lumped components and added before the circuit network of Sokal at the drain of the transistor.
as shown in Figure 3 while Figure 9(a) below which at 3.4 GHz shows a higher gain at 9.3 dB and much higher efficiency at 67 %. Figure 9(b) shows the non-overlapping current and voltage waveform thus showing switching operation.

Figure 8. (a) PAE and gain for Sokal’s equation. (b) Current and voltage at drain with Sokal’s equations

Figure 9. (a) PAE and Gain by applying S22 conjugate with Sokal’s lumped components (b) New current and voltage waveform for Sokal’s equation

3.2. Dual-Band class E PA

The result in Figure 10(b) obtained from Figure 7 the gain and efficiency is higher compared with the result in Figure 10(a) from design shown in Figure 5. Although there is a frequency shifting but nevertheless the designed amplifier is still working at Class E in both dual-band but with a narrower bandwidth of 3.43 GHz – 3.54 GHz and 3.65 GHz to 3.8 GHz achieving an above 65 % efficiency and above 8.6 dB gain. This proves the correlation of a higher efficiency and gain for the Class E by implementing the addition of the filter to remove the harmonics. The Figure 10(c) versus Figure 10(d) shows the harmonics spectrum before and after filter has been added at the OMN of the transistor respectively where it can be seen that the harmonics except the fundamental one has all been suppressed. A 1dB compression test is performed and the results is shown in Figure 10(e). This result indicates that the high input power of 22 dBm achieves the maximum efficiency but the output power is beyond 1 dB compression point. Hence going beyond the 15 dBm is going to compress the output signal in such a way that the circuit will no longer linearly amplify. But this has been shown not to be much of a problem as stated in [4] where and it showed high efficiency if the supplying voltage was large enough thus proving that such type of PA is optimum for envelope elimination and restoration (EER) transmitters (burst mode transmitters). High PAE and gain does not guarantee Class E operation. So in order to validate the Class E power amplifier we would need to view the current and voltage at the drain of the transistor whose result is shown in Figure 10(f) shows non-overlapping current-voltage waveform.
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should be for an ideal Class E PA but the voltage waveform are no longer smooth as before. But this undesirable effect does not affect out targeted efficiency, gain or frequency since the applications of Class E are mostly for non-linear based operations.

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REFERENCES

[1] M. Hayati, S. Roshani, M. K. Kazimierczuk, and H. Sekiya, “A class-e power amplifier design considering mosfet nonlinear drain-to-source and nonlinear gate-to-drain capacitances at any grading coefficient, “IEEE Transactions on Power Electronics, vol. 31, no. 11, pp. 7770-7779, 2016.

[2] N. Singhal, S. Shim, and S. Pamarti, “Class-E PA efficiency enhancement using zero voltage switching contour control,” in WAMICON 2013, pp. 1-6, 2013.

[3] R. M. Mohamed Ribate, Jamal Zbitou, Larbi El Abdellaoui, Ahmed Errkik, Mohamed Latrach, "1.25 GHz – 3.3 GHz broadband solid-state power amplifier for L and S bands applications,“ International Journal of Electrical and Computer Engineering (IJECE), vol. 9, no. 5, pp. 3633-3641, Oct 2019.

[4] K. Chen, et al., “Design of highly efficient broadband class-E power amplifier using synthesized low-pass matching Techniques,” IEEE Transactions on Microwave Theory and Techniques, vol. 59, no. 12, pp. 3162-3173, 2011.

[5] M. Hayati, A. Lotfi, M. K. Kazimierczuk, and H. Sekiya, “Generalized design considerations and analysis of class-E amplifier for sinusoidal and square input voltage waveforms,” IEEE Transactions on Industrial Electronics, vol. 62, no. 1, pp. 211-220, 2015.

[6] S. C. Cripps, “RF power amplifiers for wireless communications,” 2nd ed. Boston: Artech House, 2006.

[7] F. J. Ortega-Gonzalez, D. Tena-Ramos, M. Patiño-Gomez, J. M. Pardo-Martin, and D. Madueño-Pulido, "High-power wideband L-band suboptimum class-E power amplifier," IEEE Transactions on Microwave Theory and Techniques, vol. 61, no. 10, pp. 3712-3720, 2013.

[8] O. Ayop, M. K. A. Rahim, N. A. Murad, N. A. Samsuri, F. Zubir, and H. A. Majid, “Dual-band metamaterial perfect absorber with nearly polarization-independent,” Applied Physics A, vol. 123, no. 1, pp. 1-7, 2016.

[9] A. Wahid, M. K. A. Rahim, and F. Zubir, “Analysis of dual layer unit cell with minkowski radiating shape for reflectarray antenna on different substrate properties,” in 2010 IEEE Asia-Pacific Conference on Applied Electromagnetics (APACE), pp. 1-5, 2010.

[10] M. Hayati, A. Lotfi, M. K. Kazimierczuk, and H. Sekiya, “Analysis, design, and implementation of the class-E ZVS power amplifier with mosfet nonlinear drain-to-source parasitic capacitance at any grading coefficient,” IEEE Transactions on Power Electronics, vol. 29, no. 9, pp. 4989-4999, 2014.

[11] M. Kazimierczuk and K. Puczko, “Exact analysis of class E tuned power amplifier at any Q and switch duty cycle,“ IEEE Transactions on Circuits and Systems, vol. 34, no. 2, pp. 149-159, 1987.

[12] M. Fu, H. Y. Yin, M. Liu, and C. Ma, “Loading and power control for a high-efficiency class E pa-driven megahertz WPT system,” IEEE Transactions on Industrial Electronics, vol. 63, no. 11, pp. 6867-6876, 2016.

[13] A. Lotfi, A. Medi, A. Katsuki, F. Kurokawa, H. Sekiya, M. K. Kazimierczuk, T. Stetsugu, “Subnominal operation of class-E nonlinear shunt capacitance power amplifier at any duty ratio and grading coefficient,” IEEE Transactions on Industrial Electronics, vol. 65, no. 10, pp. 7878-7887, 2018.

[14] A. Grebennikov, N. Sokal, and M. Franco, “Switchmode RF and Microwave Power Amplifiers,” Academic Press 2012.

[15] M. Albuete, “RF Power Amplifiers,” Institution of Engineering and Technology, 2001.

[16] J. Liang, et al., “Steady-state simulation and optimization of class-E power amplifiers with extended impedance method,” IEEE Transactions on Circuits and Systems I: Regular Papers, vol. 58, no. 6, pp. 1433-1445, 2011.

[17] S. Liu, M. Liu, S. Yang, C. Ma, and X. Zhu, “A novel design methodology for high-efficiency current-mode and voltage-mode class-E power amplifiers in wireless power transfer systems,” IEEE Transactions on Power Electronics, vol. 32, no. 6, pp. 4514-4523, 2017.

[18] M. Silva-Pereira and J. C. Vaz, “A single-ended modified class-E PA with HD2 rejection for low-power RF applications,” IEEE Solid-State Circuits Letters, vol. 1, no. 1, pp. 22-25, 2018.

[19] J. Zhou, K. A. Morris, G. T. Watkins, and K. Yamaguchi, “Improved reactance-compensation technique for the design of wideband suboptimum class-E power amplifiers,” IEEE Transactions on Microwave Theory and Techniques, vol. 63, no. 9, pp. 2793-2801, 2015.

[20] A. Ershadi and A. Medi, "Investigation of integrated smooth transistor’s switching transition power amplifier—2.4-GHz realization of class-\textit{E}_{ab},“ IEEE Transactions on Microwave Theory and Techniques, vol. 65, no. 8, pp. 3046-3055, 2017.
[21] T. Sharma, P. Aflaki, M. Helaoui, and F. M. Ghannouchi, "Broadband GaN class-E power amplifier for load modulated delta sigma and 5G transmitter applications," IEEE Access, vol. 6, pp. 4709-4719, 2018.

[22] F. Norouzian and P. Gardner, "Concurrent dual-band high efficiency class-E power amplifier," in 2013 European Microwave Conference, pp. 1303-1306, 2013.

[23] F. Zubir and R. Rao Radhakrishnan, "Highly efficient power amplifier for microwave transmitter," AsiaSim 2017: Modeling, Design and Simulation of Systems, pp 736-745, 2017.

[24] D. M. Pozar, "Microwave engineering," 4th ed. Hoboken, NJ: Wiley, 2012.

[25] R. M. Mohamed Ribate, Jamal Zbitou, Larbi El Abdellaoui, Ahmed Errkik, Mohamed Latrach, Ahmed Lakhassassi, "A trade-off design of microstrip broadband power amplifier for UHF applications," International Journal of Electrical and Computer Engineering (IJECE), vol. 10, no. 1, pp. 919-927, Feb 2020.

[26] L. E. A. Amine Rachakh, Jamal Zbitou, Ahmed Errkik, Abdelali Tajmouati, Mohamed Latrach, "A novel configuration of a microstrip power amplifier based on GaAs-FET for ISM applications," International Journal of Electrical and Computer Engineering (IJECE), vol. 8, no. 5, pp. 3882-3889, Oct 2018.

[27] L. E. A. Amine Rachakh, Jamal Zbitou, Ahmed Errkik, Abdelali Tajmouati, Mohamed Latrach, "A novel design of a microstrip microwave power amplifier for DCS application using collector-feedback bias," International Journal of Electrical and Computer Engineering (IJECE), vol. 8, no. 3, pp. 1647-1653, Jun 2018.

[28] F. Norouzian, "Dual-band and switched-band highly efficient power amplifiers," Doctor of Philosophy, School of Electronic, Electrical and Computer Engineering, University of Birmingham, 2014.

[29] N. O. Sokal, "Class-E switching-mode high-efficiency tuned RF/microwave power amplifier: improved design equations," in 2000 IEEE MTT-S International Microwave Symposium Digest (Cat. No.00CH37017), vol. 2, pp. 779-782, 2000.

**BIOGRAPHIES OF AUTHOR**

**Boodhoo Kirish** received B.Eng. degree in Electronic Engineering from Infrastructure University Kuala Lumpur (IUKL), Selangor, Malaysia in 2017 and Master in Electronic and Telecommunication by taught course in 2019 at the Universiti Teknologi Malaysia (UTM), Skudai, Johor, Malaysia.

**Farid Zubir** received the B.Eng. degree in Electrical majoring in Telecommunication as well as M.Eng. (RF & Microwave) degree from the Universiti Teknologi Malaysia (UTM) in 2008 and 2010 respectively. In 2015, he then completed his Ph.D at the University of Birmingham, UK, for research into direct integration of power amplifiers with antennas in microwave transmitters. He is currently serves as a Senior Lecturer in the Department of Communication Engineering, School of Electrical Engineering, UTM. His current research interest and specialization are in the area of RF and microwave technologies including planar array antenna, dielectric resonator antenna (DRA), active integrated antenna (AIA), microstrip reflectarray antenna (MRA), millimetre wave antenna, electromagnetic band gap (EBG), artificial magnetic conductor (AMC), metamaterial and microwave amplifier. He has published over 40 articles in journals, book chapters, conference papers and proceedings.

**Mohamad Kamal A Rahim** received the B.Eng. degree in Electrical and Electronic Engineering from University of Strathclyde, UK, in 1987. In 1989, he joined the Department of Communication Engineering, Faculty of Electrical Engineering Universiti Teknologi Malaysia Kuala Lumpur as an Assistant Lecturer A. He obtained his M.Eng Science from University of New South Wales Australia in 1992 and PhD degrees in Electrical Engineering from University of Birmingham UK in 2003. After he received his Master he was appointed as a Lecturer at Faculty of Electrical Engineering. Now he is the Professor in RF and Antenna at Faculty of Electrical Engineering Universiti Teknologi Malaysia. Some of his research interest includes the areas of design of dielectric resonator antennas, microstrip antennas, RFID antennas for readers and tags, microwave circuits, EBG, artificial magnetic conductors, metamaterials, phased array antennas, computer aided design for antennas, and design of millimeter frequency antennas. He has published over 200 articles in journals and conference papers.

**Shahril Mohd Shah** obtained his B. Eng in Microwave and Communication from Multimedia University (MMU) in 2002. He received his M.Sc in Microwave Engineering and Wireless Subsystems Design from the University of Surrey, UK in 2004 and pursuing his Ph.D in Communication Engineering from the University of Birmingham, UK before graduating in 2016. He is currently a Senior Lecturer in the Department of Electronic Engineering, Faculty of Electrical and Electronic Engineering, Universiti Tun Hussein Onn Malaysia (UTHM). His research interests include, but not limited to, design of mobile devices, active and passive antennas and nonlinear characterisation of active devices.

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