Research Article

Dynamics and Robust Control of a New Realizable Chaotic Nonlinear Model

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We present a new viable nonlinear chaotic paradigm. This paradigm has four nonlinear terms. The essential features of the new paradigm have been investigated. Our new system is confirmed to have chaotic behaviors by calculating its Lyapunov exponents. The relations of the system states are displayed by a suggested new signal flow graph (SFG). The proposed SFG is discussed via some graph theory tools, and some of its hidden features are calculated. In addition, the system is realized via constructing its electronic circuit which helps in the real applications. Also, a robust controller for the system is designed with the aid of a genetic algorithm.

1. Introduction

The first noteworthy autonomous chaotic paradigm was proposed by Lorenz in 1963 to model the dynamics of the atmospheric convection with three connected differential equations [1]. Subsequent, Rossler constructed 3D chaotic paradigm with single cross-product nonlinear term [2]. Another 3D chaotic paradigm called the Chen model was constructed by Chen and Ueta in 1999, and they proved that it is a dual and not equivalent to the Lorenz model [3]. After that, in 2002, Lü, in [4], constructed an important chaotic paradigm between Lorenz and Chen models, and then the generalized Lorenz model [5] was constructed as a link of Lorenz, Chen, and Lü paradigms. Few years ago, a novel 3D chaotic paradigm with complicated chaotic behavior and interesting features was constructed by Qi et al. in [6]. During the last ten years, constructing and studying new chaotic paradigms have attracted many researchers in various fields because the chaos phenomena have been found in several modern applications such as communication algorithms, signal processing, nonlinear networks, and chemical and biological structures. In addition, several real applications come up to several new and interesting research points as chaos control techniques [7, 8] and synchronization of chaos systems [9, 10].

The 2D autonomous systems cannot have chaos features as demonstrated by Poincare–Bendixson theorem [11]. Also, in [12], the authors have proved that 3D dissipative quadratic models represented by ODEs, with total four terms at the right-hand side, cannot have chaos features. After that, in [13], Sprott suggested one quadratic nonlinear term chaotic model in which the right-hand side contains only five terms. From algebraic point of view, the system is considered the simplest chaotic model. The most interesting challenge is to design a 3D autonomous quadratic chaotic paradigm having complicated attractor entity. So, we hope to introduce a new
chaotic nonlinear model with seven terms at the right-hand side and four of them are nonlinear.

The following conditions are satisfied by the chaotic models [14, 15]: (i) very sensitive to starting conditions; (ii) have a single positive Lyapunov exponent. Due to the high capacity, high security, and high efficiency of dealing with chaotic systems, it has widely potentially utilized in nonlinear circuits, secure communications, lasers, neural networks, biological systems, and so on; then, studying chaotic nonlinear models is quite significant these days [16, 17].

Representing the complicated paradigms by their signal flow graph is very helpful. It helps in understanding the structure and the complexity of the paradigm using the tools of the graph theory [18]. In directed graph theory, finding directed cycles in the graph is known as a common source of complexity [19]. Those cycles are significant in the context of engineering structures. Specially, they are significant providers of complexity. For instance, cycles can produce positive feedback loops [20], which drive the system to be unstable. Cycles in engineering paradigms also increase the complexity of design and analyse the context of simulation convergence [19]. There are several studies in the literature on graph complexity criteria [19]. Such criteria can either directly or indirectly be linked to the values of eigenvalues of the studied graph matrices.

In real life and in process control, it is very important to control systems in order to work in a desired stable steady operating situation. All of the following are examples of the real processes that need to operate in a predetermined states, adjusting satellite orbits, controlling missile tracks in military applications, in space applications, and in industry also where it is important to control temperature, pressure, and other process variables at specific operating values. Consequently, track control methods of chaotic paradigms have taken a great attention. In [21], Yang, Chen, and Yau proposed a track controller for Lorenz structure. Their reference values were suggested to obey certain constraints which has restricted the applicability of their controller. In [22], Gao developed a track controller in such a way to avoid the constraints of the method in [21]. In [23], a novel strategy for complete and phase robust synchronizations of chaotic nonlinear systems based on single-state feedback track synchronization control technique and genetic algorithm was proposed. More studies on control of nonlinear systems can be found in [24–28]. Different control strategies can be found in [29–32].

The contribution and addition to this paper is to present a new chaotic nonlinear mathematical model. This model has applications in engineering and communications, and we will prove this by making an electronic circuit for this model. Here, we follow the same strategy to design a new track controller in order to drive the proposed chaotic system to follow any desired reference points. This control technique is designed using one state variable as a feedback variable which reduces the needed sensors and make it easy to implement in real and also minimize the cost.

The remaining parts of our work are organized as follows: the model description and its basic properties are investigated in five sections in Section 2. The proposed SFG of the system and its discussion are studied in Section 3. Designing the electronic circuit that implements the system is presented in Section 4. The method of single-state feedback control for the proposed system is presented in Section 5. The robustness of the proposed controller is studied and discussed in Section 6. The conclusion of our study is put at the end of the paper before the list of cited references.

2. System Characterization and Its Basic Features

At first, we suggest a novel three-dimensional autonomous paradigm:

\[
\begin{align*}
\dot{x}_1(t) &= a_1(x_2(t) - x_1(t)) + x_2(t)x_3(t), \\
\dot{x}_2(t) &= a_2x_2(t) - a_3x_1(t)x_3(t), \\
\dot{x}_3(t) &= a_4x_3^3(t) - a_5x_3(t),
\end{align*}
\]

(1)

where \((x_1(t), x_2(t), x_3(t)) \in \mathbb{R}^3\) and \(a_1, a_2, a_3, a_4, a_5\) are real parameters.

System (1) has the following essential dynamical features.

2.1. System (1) Generalized Hamiltonian. Smooth nonlinear system (1) is considered, given in the following formula:

\[
\dot{x} = \alpha(x) \frac{\partial H}{\partial x} + \sigma(x) \frac{\partial H}{\partial x^T},
\]

(2)

where \(x = [x_1(t), x_2(t), x_3(t)]^T\), \(H(x)\) is smooth energy function and universally positive definite, and \((\partial H/\partial x)\) is a column gradient vector of \(H(x)\).

By using energy function in quadratic formula, we have

\[
H(x) = \frac{1}{2} x^T \gamma x,
\]

(3)

where \(\gamma\) signifies a constant diagonal matrix, which is symmetric and positive definite, with respect to \((\partial H/\partial x) = \gamma x\), \(\alpha(x)\) is antisymmetric matrix representing the vector field of the workless part, and \(\sigma(x)\) is a symmetric matrix, a negative definite, representing the working or nonconservative part of the system:

\[
\begin{align*}
\alpha(x) &= [-\alpha(x)]^T, \\
\sigma(x) &= [\sigma(x)]^T.
\end{align*}
\]

(4)

Define \(H(x)\) of the model in (1) as

\[
H(x) = \frac{1}{2} \left[ \left( \frac{x_1(t)}{-a_3x_1(t)x_2(t)} \right)^2 + \left( \frac{x_2(t)}{-a_3x_3(t)} \right)^2 + \left( \frac{x_3(t)}{x_3(t)} \right)^2 \right],
\]

\[
\begin{bmatrix}
\dot{x}_1(t) \\
\dot{x}_2(t) \\
\dot{x}_3(t)
\end{bmatrix} = \begin{bmatrix}
x_1(t) \\
-x_2(t)x_3(t) \\
-x_1(t)x_2(t)
\end{bmatrix} A + B \begin{bmatrix}
x_2(t) \\
-x_3(t) \\
x_1(t)
\end{bmatrix},
\]

(5)
where

\[
A = \begin{bmatrix}
0 & \frac{1}{2} (-a_3 x_3(t)) (a_1 + x_3(t)) & -\frac{1}{2} a_3 x_1(t) x_2(t) (-a_3 x_3(t)) \\
\frac{1}{2} (-a_3 x_3(t)) (a_1 + x_3(t)) & 0 & -\frac{1}{2} a_3 x_1(t) \\
-\frac{1}{2} a_3 x_1(t) x_2(t) (-a_3 x_3(t)) & \frac{1}{2} a_3 x_1(t) & 0 
\end{bmatrix},
\]

\[
B = \begin{bmatrix}
a_1 a_3 x_3(t) x_2(t) & \frac{1}{2} (-a_3 x_3(t)) (a_1 + x_3(t)) & \frac{1}{2} a_3 x_1(t) x_2(t) (-a_3 x_3(t)) \\
\frac{1}{2} (-a_3 x_3(t)) (a_1 + x_3(t)) & -a_2 a_3 x_3(t) & -\frac{1}{2} a_3 x_1(t) \\
\frac{1}{2} a_3 x_1(t) x_2(t) (-a_3 x_3(t)) & \frac{1}{2} a_3 x_1(t) & -a_5 
\end{bmatrix}
\] (6)

The existence of the Hamilton in model (1) implies its ability to model natural phenomena.

2.2. Invariance and Symmetry of the Proposed Model. For system (1), the transformation \((x_1(t), x_2(t), x_3(t)) \rightarrow (-x_1(t), -x_2(t), x_3(t))\) implies that the system is invariant.

Then, if \((x_1(t), x_2(t), x_3(t))\) is a solution of model (1), then \((-x_1(t), -x_2(t), x_3(t))\) is a solution of the same model too.

2.3. Dissipation of Proposed Model (1). The divergence of proposed paradigm (1) is

\[
\nabla \cdot \mathbf{V} = \frac{\partial \mathbf{x}_1(t)}{\partial x_1(t)} + \frac{\partial \mathbf{x}_2(t)}{\partial x_2(t)} + \frac{\partial \mathbf{x}_3(t)}{\partial x_3(t)}
\]

\[
= -a_1 + a_2 - a_5.
\]

Then, proposed chaotic paradigm (1) is dissipative such that

\[-a_1 + a_2 - a_5 < 0.\] (8)

2.4. Fixed Point and Its Stability of Proposed Model (1). Solving the following system of equations leads to the equilibria of system (1):

\[
0 = a_1 x_2(t) - x_1(t),
0 = a_2 x_2(t) - a_3 x_1(t) x_3(t),
0 = a_4 x_1(t) x_3(t) - a_5 x_3(t).
\]

System (1) has a trivial fixed point \(E_0 = (0, 0, 0)\).

In order to examine the stability of \(E_0\), the Jacobian matrix of proposed model (1) at \(E_0\) is

\[
J_{E_0} = \begin{bmatrix}
-a_1 & a_1 & 0 \\
0 & a_2 & 0 \\
0 & 0 & -a_5 
\end{bmatrix},
\]

the characteristic equation of \(J_{E_0}\) is

\[
(\lambda + a_1)[\lambda^2 + \lambda (a_5 - a_2) - a_2 a_5] = 0,
\]

and as a result, the characteristic equation of \(J_{E_0}\) has the following three eigenvalues:

\[
\lambda_1 = -a_1, \lambda_2 = a_5 - a_2, \lambda_3 = a_2 a_5 = 0.
\]

By applying Routh–Hurwitz theorem, the trivial fixed point is stable if and only if

\[
a_1 > 0, a_5 - a_2 > 0, \text{ and } -a_2 a_5 > 0.
\]

So, the constraints making the trivial fixed point stable are

\[
a_1 > 0, a_5 > a_2, \text{ and } a_2 a_5 < 0,
\]

otherwise it is unstable.

2.5. Calculating Lyapunov Exponents for Proposed Model (1). Proposed model (1) can be written in vector notation as

\[
\dot{X}(t) = h(X(t); \eta).
\]

Such that \(X(t) = [x_1(t), x_2(t), x_3(t)]^T\) presents the vector of state space, \(h = [h_1, h_2, h_3]^T\), \(\eta\) presents the parameters, and \([\ldots]^T\) signifies matrix transpose operation. The deviations from the \(X(t)\) trajectory are given in the following equation:
\[ \delta X(t) = J_{ij}(X(t); \eta)\delta X, \quad i, j = 1, 2, 3, \]  
\[ J_{ij} = (\partial h_i/\partial x_j) \]

where \( J_{ij} \) is the Jacobian matrix and takes the following form:

\[ J_{ij} = \begin{pmatrix} -a_1 & a_1 + x_1(t) & x_1(t) \\ -a_2 x_3(t) & a_2 & -a_3 x_3(t) \\ 2a_4 x_1(t) & 0 & -a_5 \end{pmatrix}. \]  

(17)

The Lyapunov exponents \( L_i \) of the system are defined by

\[ L_i = \lim_{t \to \infty} \frac{1}{t} \log \frac{\delta x_i(t)}{\delta x_i(0)}. \]  

(18)

Numerically solve equations (14) and (15) simultaneously to find \( L_i \). Order 4 Runge–Kutta algorithm is utilized to estimate \( L_i \).

The system parameters are selected as follows: \( a_1 = 10, a_2 = 5, a_3 = 4, a_4 = 2, \) and \( a_5 = 3 \) where the initial values are chosen as \( x_1(0) = 1, x_2(0) = 2, \) and \( x_3(0) = 3 \). The Lyapunov exponents are estimated as follows: \( L_1 = 1.01, L_2 = 0, \) and \( L_3 = -12.5 \).

This implies that our proposed system (1) for this selection of the parameters \( a_1, a_2, a_3, a_4, \) and \( a_5 \) is a chaotic paradigm because it has one positive Lyapunov exponent.

Figure 1 proves that our proposed model (1) is chaotic. Solving system (1) numerically, for specific selections of the parameter values, it is clear that it has chaotic behavior in specific domains where initially nearby trajectories break away exponentially with time. For example, Figure 1(a) displays two such numerically evaluated solutions of (1), where we give only the \((t, x_1(t))\) plot. The chaotic behavior of those solutions is confirmed from the fact that the two initially nearby orbits break away from each other exponentially at about \( t \approx 15 \). As shown in Figure 1(b), model (1) has a chaotic attractor. In Figure 1(b), we plot the motion in the 3-dimensional space \((x_1(t), x_2(t), x_3(t))\).

In Figure 2, we fix \( a_2 = 5, a_1 = 4, a_4 = 2, \) and \( a_5 = 3 \) and vary \( a_1 \in [1, 30] \). From Figure 2, it is clear that system (1) has periodic solution when \( a_1 \in [1, 8.4] \). The chaotic attractors appear when \( a_1 \in [8.4, 19.3] \). If \( a_1 \in [19.3, 30] \), our system has fixed point solutions. Figure 2 proves that our new system contains chaotic solutions over a wide period \( a_1 \in [8.4, 19.3] \). As we did with the \( a_1 \) parameter, we did with the rest of the parameters. And because we got almost the same results, we will not display the results for the rest of the parameters.

In Figure 2, we find chaotic attractors, periodic attractors, and fixed point solutions of system (1). To check this, we have solved numerically (16) (using, e.g., Mathematica 7 software) in several cases and excellent agreements are found with the results of Figure 2. For example, choosing \( a_2 = 5, a_3 = 4, a_4 = 2, \) and \( a_5 = 3, \) with the initial conditions \( t_0 = 0, x_1(0) = 1, x_2(0) = 2, \) and \( x_3(0) = 3, \) and when \( a_1 = 7, \) the solution of system (1) has periodic solution trivial fixed point (see Figure 3(a)), chaotic attractor when \( a_1 = 10 \) as in Figure 3(b). In Figure 3(c), \( a_1 = 27, \) the solution is fixed point.

### 3. System Signal Flow Graph

Representing the complex systems graphically is useful for understanding the relationship between its components. Our system components are its direct state variables \( x_1, x_2, \) and \( x_3 \) in addition to the combined three states \( x_1^2, x_1 x_3, \) and \( x_2 x_3. \)

Each state variable is represented by a vertex in the digraph \( G \) of system (1). The edge \((u, v) \in G \) iff \((\partial v/\partial u) \neq 0 \). Then, the adjacency matrix of \( G \) is an image of the relationships between the system state variables of system (1). Figure 4 shows the proposed graph of the studied system.

The following is the weighted adjacency matrix, \( A(G) \), of the system’s proposed graph:

\[
A(G) = \begin{bmatrix}
-x_1 & 0 & 0 & 0 & 1 & 1 & 0 \\
0 & a_1 & 0 & a_2 & 0 & 0 & 1 \\
0 & 0 & -a_3 & 0 & 1 & 1 & 0 \\
0 & 0 & 0 & a_4 & 0 & 0 & 0 \\
0 & -a_5 & 0 & 0 & 0 & 0 & 0 \\
1 & 0 & 0 & 0 & 0 & 0 & 0
\end{bmatrix}.
\]  

(19)

The energy of the matrix in (9) can be used to compute the energy of the digraph \( G \) (see [19]). To compute the energy of the proposed graph, we follow the method explained in [19] (page 6).

Firstly, formulate the adjacency matrix of the system graph \( M \) where

\[ M_{ij} = \begin{cases} 1, & \text{for any edge } (u, v), \ u \neq v \text{ of the graph;} \\ 0, & \text{otherwise.} \end{cases} \]  

(20)

Then,

\[
M(G) = \begin{bmatrix}
x_1 & 0 & 0 & 0 & 1 & 1 & 0 \\
x_2 & 1 & 0 & 0 & 0 & 0 & 1 \\
x_3 & 0 & 0 & 0 & 1 & 1 & 0 \\
x_1^2 & 0 & 0 & 1 & 0 & 0 & 0 \\
x_1 x_3 & 0 & 1 & 0 & 0 & 0 & 0 \\
x_2 x_3 & 1 & 0 & 0 & 0 & 0 & 0
\end{bmatrix}.
\]  

(21)

The energy \( E_G \) of the graph \( G \) is calculated via the following formula [19]:

\[ E_G = \left( 1/|E| \right) \sum_{k=1}^{E} w_k \sum_{i} \text{SVD}(M(G)), \]  

(22)

where \(|E|\) is the number of edges in \( G \), \( w_{|E|} \) is the edge weights, and \( \text{SVD}(M(G)) \) is a vector of singular values of matrix. For more details about graph energy, see [19].

Let \( \lambda_1, \lambda_2, \ldots, \lambda_n \) are the eigenvalues of the matrix \( M^T M \), with repetitions. Order these so that \( \lambda_1 \geq \lambda_2 \geq \cdots \geq \lambda_n \geq 0 \), assuming \( v_1 = \sqrt{\lambda_1} \), then \( v_1 \geq v_2 \geq \cdots \geq v_n \geq 0 \), and they are the components of the SVD. Then,
Figure 1: (a) Two numerically calculated solutions of (1) for $a_1 = 10, a_2 = 5, a_3 = 4, a_4 = 2,$ and $a_5 = 3$ with $t_0 = 0, x_1(0) = 1, x_2(0) = 2,$ and $x_3(0) = 3$ (solid curve) and $x_1(0) = 1.001, x_2(0) = 2,$ and $x_3(0) = 3.001$ (dotted curve). Note the exponential separation that becomes clear at $t = 15$, clearing the chaotic manner of the system orbits. (b) 3-dimensional chaotic attractor in $(x_1(t), x_2(t), x_3(t))$ space.

![Graph showing phase portrait](image)

**Figure 2:** $L_1, L_2,$ and $L_3$ versus $a_1, a_2$ in [1, 30] and $a_3 = 5, a_4 = 4, a_5 = 2,$ and $a_6 = 3$ with the same initial conditions in Figure 1.

SVD $\left( M \left( \mathcal{S} \right) \right) = [3.5321, 2.3473, 1.0, 1.0, 0, 12061]$.  

Then, $\mathcal{E}_p = 4.5$, that can be used as measure of the system complexity.

### 4. System Realization Using NI Multisim

In this section, we realize the studied system using NI Multisim and its electronic circuit is designed as shown in Figure 5. The circuit consists of three integrators symbolized as X1, X2, and X3 all of which are constructed using the 741 OP AMP; three summers S1, S2, and A3 each of which has three inputs and one output; two multipliers symbolized with X1X3, X1X1, and X2X3 each of which has two inputs and one output; three 1 micro Farad capacitors C1, C2, and C3 where it is initially charged by 1, 2, and 3 volts, respectively, to realize the initial conditions of the studied system; and ten resistors R1, R2, ..., R10, where R1, R3, R5, R7, R8, R9, and R10 are equal 10 kohms and R2, R4, and R6 are equal 100 kohms. The input and output gains of the summers are designed as follows (Table 1) in order to realize the studied system. Figure 6 shows the phase portrait of the state variable $x_2$ with respect to the state variable $x_1$. Figure 7 shows the phase portrait of the state variable $x_3$ with respect to the state variable $x_1$. Figure 8 shows the phase portrait of the state variable $x_3$ with respect to the state variable $x_2$.

Table 2 shows the designed values of input/output gains of the used multipliers.

### 5. Single-State Feedback Control for the Proposed System

#### 5.1. Controller Design

In this section, we designed a reference point-based single-state feedback controller. The suggested controller will drive the states of the proposed chaotic model to follow the desired predetermined reference values. The proposed controller’s input consists of the output and the states of the chaotic system. The output of the controller is used as an input of the controlled chaotic system.

In [21], the proposed controller was depended on the sliding-mode technique and the Lorenz system states were derived to track the reference values but under some constraints which limit its real applications. In [22], the author proposed a track controller by which the Lorenz system states were derived to follow any of their predetermined reference values. In this work, a reference value single-state feedback controller is to be constructed in such a way that the proposed chaotic model states will be derived to track any desired reference values without any constraints.

Here, it is proposed that the state $x_2$ of the studied system is the only state that can be easily measured. For studied system (1), a novel reference point-based single-state feedback controller is designed as follows:

\[
C_1 = -a_1 x_2 + a_1 x_1 - x_2 x_3 x_5, \\
C_2 = k (x_2 - x_3) - a_2 x_2 + a_3 x_1 x_3, \\
C_3 = -a_4 x_1 + a_5 x_3.
\]

(24)
where \( x_{ir} \) is the desired reference value of the system state \( x_i \) for all \( i \in \{1, 2, 3\} \) and \( k \) is the controller gain.

In (24), the closed-loop feedback is constructed only using the second state variable \( x_2 \). Hence, it is called single-state feedback controller.

The controlled system via the proposed controller becomes

\[
\begin{align*}
\frac{dx_1}{dt} &= a_1 x_1 - a_4 x_1 x_3 + C_1, \\
\frac{dx_2}{dt} &= a_2 x_2 - a_3 x_1 x_3 + C_2, \\
\frac{dx_3}{dt} &= a_4 x_2^2 - a_5 x_3 + C_3.
\end{align*}
\]

(25)

Assume that \( x_{ir} \) denotes the desired reference value of the state variable \( x_i \) where \( i = 1, 2, 3 \). And let \( \{E_i = x_i - x_{ir}; i = 1, 2, 3\} \) is the errors set between the system state variable and their references. Then, putting \( \dot{x}_1 = E_1 + x_{ir}, \dot{x}_2 = E_2 + x_{ir}, \) and \( \dot{x}_3 = E_3 + x_{ir} \) in (25), the control error dynamical system can be derived as follows:

\[
\begin{align*}
\frac{dE_1}{dt} &= a_1 E_2 - a_4 E_1 + E_2 E_3 + x_{ir} E_2 + x_{ir} E_3, \\
\frac{dE_2}{dt} &= (a_2 + k) E_2 - a_3 E_1 E_3 - a_3 x_{ir} E_1 - a_3 x_{ir} E_3, \\
\frac{dE_3}{dt} &= a_4 E_1^2 + 2a_4 x_{ir} E_1 - a_5 E_3.
\end{align*}
\]

(26)

It is clear that the \( E_o = (0, 0, 0) \) is an equilibrium of error dynamical system (26) and its Jacobian matrix can be written as

\[
\begin{align*}
J(E) &= \begin{bmatrix}
-a_1 & a_1 + E_3 + x_{ir} & E_2 + x_{ir} \\
-a_3 E_1 - a_3 x_{ir} & (a_2 + k) & -a_3 E_1 - a_3 x_{ir} \\
2a_4 E_1 + 2a_4 x_{ir} & 0 & -a_5
\end{bmatrix}, \\
J(E_o) &= \begin{bmatrix}
-a_1 & a_1 + x_{ir} & x_{ir} \\
-a_3 x_{ir} & (a_2 + k) & -a_3 x_{ir} \\
2a_4 x_{ir} & 0 & -a_5
\end{bmatrix}.
\end{align*}
\]

(27)
If the controller gain $k$ can be calculated such that the eigenvalues of the Jacobian matrix 16 are all stable, the control errors $E_1$, $E_2$, and $E_3$ will be stable asymptotically at its equilibrium $E_0 = (0, 0, 0)$. This implies that the system states $x_1$, $x_2$, and $x_3$ will follow their desired reference values $x_{1r}$, $x_{2r}$, and $x_{3r}$, respectively.
Then, our task is to calculate the suitable value of the gain $k$. Our result is written in the following result.

**Theorem 1.** Let $\Omega = a_3 x_3^2 + a_1 a_3 x_3 - a_1 a_2 + a_1 a_5 - a_2 a_5 - 2a_4 x_1 x_2$, $\Phi = a_3 a_4 x_3^2 - a_1 a_2 a_5 + 2a_3 a_4 x_3 x_1^2 + a_1 a_5 x_3 + 2a_1 a_4 a_4$, $\Delta = (a_1 + a_5)$, and $\beta = (-\Omega - a_1^2 - a_2^2 + a_1 a_2 - a_2 a_5 - a_1 a_5 + a_2 a_5 - a_4 x_1 x_2)$, and $c = (\Omega a_5 + \Omega a_1 - \Phi - a_2)$. The states of studied system (1) can follow any desired pre-determined values $x_1, x_2$, and $x_3$ via the proposed controller 12, if the controller gain $k$ is adjusted such that

$$k < \min \left\{ \frac{(a_1 - a_2 + a_5) - \Phi}{a_1 a_5 - 2a_4 x_2 x_1}, \frac{-b - \sqrt{b^2 - 4ac}}{2a} \right\}. \quad (28)$$

**Proof.** Studied system (1) has the following characteristic equation at its equilibrium point:

\[
\Delta(\lambda) = \begin{vmatrix}
\lambda + a_1 & -a_1 - x_3 & -x_2 \\
\lambda + (a_2 + k) a_3 x_3 & a_3 x_3 & 0 \\
-2a_4 x_1 & 0 & \lambda + a_5 \\
\end{vmatrix} = 0,
\]

\[
\Delta(\lambda) = \begin{vmatrix}
\lambda + a_1 & -a_1 - x_3 & -x_2 \\
\lambda + (a_2 + k) a_3 x_3 & a_3 x_3 & 0 \\
-2a_4 x_1 & 0 & \lambda + a_5 \\
\end{vmatrix} = 0.
\]

Let $\beta_2 = (a_1 - k - a_5 + a_4), \beta_1 = -(a_1 + a_5)k + \Omega$, where $\Omega = a_3 x_3^2 + a_1 a_3 x_3 - a_1 a_2 + a_1 a_5 - a_2 a_5 - 2a_4 x_1 x_2$ and

\[
\beta_0 = a_3 a_5 x_3^2 - ka_1 a_5 - a_1 a_2 a_5 + 2a_3 a_4 x_3 x_1^2 + 2ka_4 x_2 x_1 + a_1 a_5 x_3 + 2a_1 a_4 x_3 x_1 + 2a_3 a_4 x_2 x_1
\]

where $\Phi = a_3 a_4 x_3^2 - a_1 a_2 a_5 + 2a_3 a_4 x_3 x_1^2 + a_1 a_5 x_3 + 2a_1 a_4 x_3 x_1 + 2a_3 a_4 x_2 x_1.$

Then, $\Delta(\lambda)$ can be written as

$$\lambda^3 + \beta_2 \lambda^2 + \beta_1 \lambda + \beta_0 = 0. \quad (31)$$

Applying Routh–Hurwitz stability criterion, the eigenvalues of (31) have negative real parts if and only if $\beta_2 > 0$, $\beta_0 > 0$, and $\beta_2 \beta_1 - \beta_0 > 0$.

From $\beta_2 > 0$ and $\beta_0 > 0$, it is clear that

$$k < \begin{cases} (a_1 - a_2 + a_5), & \text{and} \\
\frac{\Phi}{a_1 a_5 - 2a_4 x_2 x_1}. & \end{cases} \quad (32)$$

Note that

$$\beta_2 \beta_1 - \beta_0 = (a_1 - k - a_2 + a_5) (-(a_1 + a_5)k + \Omega) - (k(2a_4 x_2 x_1 - a_1 a_5) + \Phi), \quad (33)$$

$$= (a_1 - k - a_2 + a_5) (-(a_1 + a_5)k + \Omega) - (k(2a_4 x_2 x_1 - a_1 a_5) + \Phi)$$

$$= (a_1 + a_5)k^2 + k(-\Omega - a_1^2 + a_2 a_5 - a_1 a_5 - 2a_4 x_1 x_2)$$

$$+ (\Omega a_5 + \Omega a_1 - \Phi - a_2)$$

$$= ak^2 + bk + c, \quad (34)$$
where \( a = (a_1 + a_3), \quad b = (-\Omega - a_1^2 - a_3^2 + a_1 a_2 - a_1 a_5 + a_2 a_5 - 2a_4 x_{1r} x_{2r}), \) and \( c = (\Omega a_5 + \Omega a_1 - \Phi - \Omega a_3). \)

From (33) and \( \beta^2 \beta_1 - \beta_0 > 0, \) we can derive that

\[
\left( k - \frac{-b + \sqrt{b^2 - 4ac}}{2a} \right) \left( k - \frac{-b - \sqrt{b^2 - 4ac}}{2a} \right) > 0, \tag{35}\]

which implies that

\[
k < \min \left\{ \frac{(a_1 - a_3)}{a_1 a_5 - 2a_4 x_{1r} x_{2r}}, \frac{\Phi}{a_1 a_5 - 2a_4 x_{1r} x_{2r}}, \frac{-b - \sqrt{b^2 - 4ac}}{2a} \right\}, \tag{36}\]

which completes the proof. \( \square \)

5.2. Case Studies of Reference Value-Based Control of the Studied System

Case 1. \( x_{1r} = x_{2r} = x_{3r} = 0 \)

Applying Theorem 1, the controller gain can be calculated and we can select it \( k = -8. \) Proposed controller (24) is
Case 2. Applying theorem 1, the controller gain can be calculated and we can select it $k = -50$. Proposed controller (24) is applied to studied system (1) at $t = 30$ secs. Figure 10 shows the system states before and after applying control. It is obvious that the proposed controller drives the state variables to follow their reference values after applying it immediately.

Case 3. $x_{1r} = 10$, $x_{2r} = -10$, $x_{3r} = 20$

Applying Theorem 1, the controller gain can be calculated and we can select it $k = -60$. Proposed controller (24) is applied to studied system (1) at $t = 30$ secs. Figure 11 shows the system states before and after applying control. It is obvious that the proposed controller drives the state variables to follow their reference values after applying it immediately.

### 6. Robust Controller

In this section, a tracking robust controller is to be designed. Since in practice, the uncertainties are unavoidable matter, then it is important to design a robust single-state feedback tracking controller for the studied system.

#### 6.1. Robust Track Controller Algorithm Design

Suppose the system parameters have some perturbations. The fuzzy studied system can be written in the following format:

\[
\begin{align*}
\frac{dx_1}{dt} &= (a_1 + \Delta a_1)x_2 - (a_1 + \Delta a_1)x_1 + x_2x_3 + C_1, \\
\frac{dx_2}{dt} &= (a_2 + \Delta a_2)x_2 - (a_2 + \Delta a_2)x_1x_3 + C_2, \\
\frac{dx_3}{dt} &= (a_3 + \Delta a_3)x_1^2 - (a_3 + \Delta a_2)x_1 + C_3.
\end{align*}
\]

Applying theorem 1, the controller gain can be calculated and we can select it $k = -50$. Proposed controller (24) is applied to studied system (1) at $t = 30$ secs. Figure 10 shows the system states before and after applying control. It is obvious that the proposed controller drives the state variables to follow their reference values after applying it immediately.

Simplifying (38), we get

\[
\begin{align*}
\frac{dx_1}{dt} &= a_1x_2 - a_1x_1 + x_2x_3 + \Delta a_1(x_2 - x_1) + C_1, \\
\frac{dx_2}{dt} &= a_2x_2 - a_3x_1x_3 + \Delta a_2x_2 - \Delta a_3x_1x_3 + C_2, \\
\frac{dx_3}{dt} &= a_4x_1^2 - a_5x_3 + \Delta a_4x_1^2 - \Delta a_5x_3 + C_3.
\end{align*}
\]

The uncertainties are collected in a column vector $u = (u_1, u_2, u_3)^T$ where $u_1 = \Delta a_1(x_2 - x_1)$, $u_2 = \Delta a_2x_2 - \Delta a_3x_1x_3$, and $u_3 = \Delta a_4x_1^2 - \Delta a_5x_3$. Applying designed controller (24) upon system (39), the new dynamics of the tracking error will be as

\[
\begin{align*}
\frac{dE_1}{dt} &= a_1E_2 - a_1E_1 + E_2E_3 + x_3E_2 + x_2E_3 + u_1, \\
\frac{dE_2}{dt} &= (a_2 + k)E_2 - a_1E_1E_3 - a_3x_3E_1 - a_3x_1E_3 + u_2, \\
\frac{dE_3}{dt} &= a_4E_1^2 + 2a_4x_1E_1 - a_5E_3 + u_3.
\end{align*}
\]
Figure 9: State dynamics under the track control method with reference \((0, 0, 0)\) and the controller gain \(k = -8\), where the controller is applied after 30 secs. (a) The state variable \(x_1\); (b) the state variable \(x_2\); (c) the state variable \(x_3\); (d) track control errors \(E_1\), \(E_2\), and \(E_3\).

Figure 10: State dynamics under the track control method with reference \((10, -10, 20)\) and the controller gain \(k = -50\), where the controller is applied after 30 secs. (a) The state variable \(x_1\); (b) the state variable \(x_2\); (c) the state variable \(x_3\); (d) track control errors \(E_1\), \(E_2\), and \(E_3\).
fi"hatcanbewrittenas
\[ dE_1 \begin{bmatrix} \frac{dr}{dt} \\ \frac{dr}{dt} \\ \frac{dr}{dt} \end{bmatrix} = \begin{bmatrix} -a_1 \ 0 \ 0 \\ -a_3x_{3r} \ (a_2 + k) \ -a_3x_{1r} \\ 2a_4x_{1r} \ 0 \ -a_5 \end{bmatrix} \begin{bmatrix} x_1 \\ x_2 \\ x_3 \end{bmatrix} + \begin{bmatrix} 0 \\ 0 \\ -a_5 \end{bmatrix} \begin{bmatrix} E_1 \\ E_2 \\ E_3 \end{bmatrix} + \begin{bmatrix} a_4x_1^2 \\ a_5x_2^2 \end{bmatrix} \]

Let

\[ E = \begin{bmatrix} E_1 \\ E_2 \\ E_3 \end{bmatrix}, \]

\[ A = \begin{bmatrix} -a_1 \ (a_1 + x_{3r}) \ x_{2r} \\ -a_3x_{3r} \ (a_2 + k) \ -a_3x_{1r} \\ 2a_4x_{1r} \ 0 \ -a_5 \end{bmatrix}, \]

\[ U = \begin{bmatrix} U_1 \\ U_2 \\ U_3 \end{bmatrix} = \begin{bmatrix} E_2E_3 + u_1 \\ -a_3E_1E_3 + u_2 \\ a_4E_1^2 + u_3 \end{bmatrix}. \]

Then, the Laplace transformation of the track control error system \( \dot{E} = AE + U \) is given as follows:

\[ E(s) = (sI - A)^{-1}U(s). \]

Since the controller gain has no effect upon the uncertain terms \( U_1 \) and \( U_3 \), an improvement to the single-state feedback controller is designed as follows:

\[ C_1 = k_1(x_2 - x_{2r}) - a_1x_{2r} + a_1x_{1r} - x_{2r}x_{3r}, \]

\[ C_2 = k_2(x_2 - x_{2r}) - a_2x_{2r} + a_3x_{1r}x_{3r}, \]

\[ C_3 = k_3(x_2 - x_{2r}) - a_4x_1^2 + a_5x_{3r}. \]

Utilizing proposed robust controller (43) with disturbed system (39), the closed-loop track control error dynamics are given as

.png
\[
\begin{align*}
\frac{dE_1}{dt} &= k_1E_2 + a_1E_1 + x_{3r}E_2 + x_{3r}E_3 + u_1, \\
\frac{dE_2}{dt} &= (k_2 + a_2)E_2 - a_3E_1E_3 - a_3x_{3r}E_1 - a_3x_{3r}E_3 + u_2, \\
\frac{dE_3}{dt} &= k_3E_2 + a_4E_1^2 + 2a_4x_{1r}E_1 - a_3E_3 + u_3.
\end{align*}
\]

That can be rewritten in a compact format as \( \dot{E} = BE + U \) which equal the system

\[
\begin{bmatrix}
\frac{dE_1}{dt} \\
\frac{dE_2}{dt} \\
\frac{dE_3}{dt}
\end{bmatrix} =
\begin{bmatrix}
-a_1 & \left( k_1 + a_1 + x_{3r} \right) & x_{2r} \\
-a_3x_{3r} & \left( a_2 + k_2 \right) & -a_3x_{1r} \\
2a_4x_{1r} & k_3 & -a_5
\end{bmatrix}
\begin{bmatrix}
E_1 \\
E_2 \\
E_3
\end{bmatrix}
+ \begin{bmatrix}
E_2E_3 + u_1 \\
-a_5E_1E_3 + u_2 \\
a_4E_1^2 + u_3
\end{bmatrix}.
\]

6.2. Numerical Simulation for the Robust Track Controller.

In the following simulations, the disturbances are taken as

\[
\begin{align*}
u_1 &= \sin(2\pi(\omega_1 - 1)) + \text{noise}; \\
u_2 &= \sin(4\pi\omega_2) + \text{noise}; \\
u_3 &= \sin(6\pi\omega_3).
\end{align*}
\]

where noise = \( n \ast \text{(random\_number)} \), \( n = s / (10^{\text{snr}/20}) \), snr is the signal to noise ratio that set as snr = 200 log (s/n) = 100, and \( s \) is the standard deviation of \( x_2 \).

For illustration, the references are selected to be \( x_{1r} = -2, x_{2r} = 40, \) and \( x_{3r} = -60 \). Using FFT, the dominant frequencies of \( x_2 \) are selected as \( f_1 = 0.206653 \) Hz; \( f_2 = 0.319979 \) Hz; \( f_3 = 0.333311 \) Hz; \( f_4 = 0.786614 \) Hz; \( f_5 = 0.293313779 \) Hz; \( f_6 = 0.213319112 \) Hz; \( f_7 = 0.166655556 \); \( f_8 = 0.193320445 \) and \( f_9 = 0.219985334 \). Figure 12 displays the spectrum of \( x_2 \) using the FFT method.

The selected dominant frequencies are used to construct fitness function (46). \( \theta \) is set to equal 3. Figure 13 shows the optimization process via GA. The selected gains are \( k_1 = -116.67; k_2 = -332; k_3 = -68 \). Figure 14 shows the system response before and after control with the corresponding track errors. The controller drives the states to follow the reference values: \( x_{1r} = x_{2r} = x_{3r} = 0 \). Figure 15 shows the system response before and after control with the corresponding track errors. The controller drives the states to follow the reference values: \( x_{1r} = -5; x_{2r} = 5; x_{3r} = -6 \).
Figure 12: Amplitude versus frequencies of $x_2$ spectrum via FFT.

Figure 13: Fitness value versus generations in GA optimization process.

Figure 14: Continued.
7. Conclusion

In this work, the dynamics of a new proposed chaotic model have been studied. The new proposed model chaotic behaviors have been proved by calculating its Lyapunov exponents. The proposed model has been studied via discussing its symmetry and invariance, dissipativity, and the stability of its fixed point plus its Lyapunov exponents. The proposed model has been confirmed to be chaotic. The proposed chaotic model complexity has been measured using its SFG. The proposed chaotic model has been confirmed to be realizable via constructing a real electronic circuit that simulate its behavior. In addition, a new single-state feedback controller has been designed in order to

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**Figure 14:** The system response before and after control with $x_{1r} = x_{2r} = x_{3r} = 0$: (a) the state variable $x_1$ before and after control; (b) state variable $x_2$ before and after control; (c) the state variable $x_3$ before and after control; (d) the track errors before and after control.

**Figure 15:** The system response before and after control with $x_{1r} = -5; x_{2r} = 5; x_{3r} = -6$: (a) the state variable $x_1$ before and after control; (b) the state variable $x_2$ before and after control; (c) the state variable $x_3$ before and after control; (d) track errors before and after control.
operate the system such that its states can follow a pre-determined reference value. The robustness of the proposed controller has been discussed. The proposed robust controller has been constructed with the aid of the genetic algorithm. For future work, we suggest utilizing the proposed model in real applications such as secure communication applications.

Data Availability
No data were used to support the findings of this study.

Conflicts of Interest
The authors have no conflicts of interest regarding the publication of the paper.

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