Physical-layer network coding: Tutorial, survey, and beyond

Soung Chang Liew a,*, Shengli Zhang b, Lu Lu a

a Department of Information Engineering, The Chinese University of Hong Kong, Hong Kong
b Department of Communication Engineering, Shenzhen University, China

1. Introduction

The concept of physical-layer network coding (PNC) was originally proposed in [1] as a way to exploit the network coding operation [2,3] that occurs naturally in superimposed electromagnetic (EM) waves. It is a simple fact in physics that when multiple EM waves come together within the same physical space, they add. This additive mixing of EM waves is a form of network coding, performed by nature. Alternatively, the additive network coding operation can be transformed and mapped to other forms of network coding after reception. Exploiting these facts turns out to have profound and fundamental ramifications.

In many wireless communication networks today, interference is treated as a destructive phenomenon. When multiple transmitters transmit radio waves to their respective receivers, a receiver receives signals from its transmitter as well as from other transmitters. The radio waves from the other transmitters are often treated as interference that corrupts the intended signal. In Wi-Fi networks, for example, when multiple nodes transmit together, packet collisions occur and none of the packets can be received correctly.

As originally proposed in [1], PNC was an attempt to turn the situation around. By exploiting the network coding operation performed by nature, the “interference” could be put to good use. In a two-way relay channel (TWRC), for example, by allowing the two end nodes to transmit simultaneously to the relay and not treating this...
as collision, PNC can boost the system throughput by 100% [1].

To our knowledge, the same idea as PNC for application in TWRC was also independently proposed in [4]. Ref. [1], however, went beyond TWRC to discuss the application of PNC in general network topologies. In addition, the implications of PNC for MAC (medium access control) protocols and network-layer designs were also discussed in [1]. The potential benefit of network coding taking into account the characteristics of the multiple-access channel was investigated in [5] from an information-theoretic angle. Unidirectional multicast communication was the focus in [5], whereas bidirectional unicast communication was the focus in [1,4]. In [1,4,5], the relay maps the weighted sum of the simultaneously received signals to another form of network coding before relaying the information. Ref. [6] proposed and implemented a simple version of PNC called Analog Network Coding (ANC) in which the weighted sum is simply amplified and forwarded. The same idea was proposed for application in the satellite network in an earlier paper in 1998 [7]. In this article, we will broadly refer to all the above schemes that exploit simultaneous reception of signals to effect network coding operations as PNC schemes.

Since 2006, many researchers have made contributions that advance the understanding of PNC. The flavors of the research fall into three general categories: (1) communication-theoretic studies; (2) information-theoretic analyses; and (3) network and protocol designs. PNC raises many new interesting issues on each of the three fronts. For example, an interesting issue from the communications standpoint is the extent to which synchronization of the simultaneous transmissions by multiple transmitters to a receiver is required in a PNC system. An interesting information-theoretic issue is the extent to which the cut-set bound on the information capacity can be approached when PNC is applied to TWRC. Interesting networking issues include how to apply PNC in a network setting with many sources and destinations, and how to design multiple-access protocols to exploit the fact that not all interferences are bad in a wireless network operated with PNC.

The purpose of the present paper is fourfold. First, we give a brief tutorial on the basic concept of PNC and related key issues. Second, we survey and discuss recent results on the above three fronts. Third, we examine a critical issue in PNC: synchronization. It has been a common belief that PNC requires tight synchronization. We present some recent results suggesting that PNC may actually benefit from asynchrony. Fourth, we put forth the idea of “optical PNC”. We provide an example showing that the throughput of a passive optical network (PON) could potentially be raised by 100% with optical PNC. Our target audience includes new entrants in the area, as well as researchers and engineers that need to see the bigger picture of PNC.

Throughout this article, the term “capacity” is used in the information-theoretic sense. That is, by “capacity”, we mean information-theoretic capacity in which a data rate below the capacity can be achieved with arbitrarily low error probability with channel-coded packets of large length. The term “throughput” is used in the networking sense. In a network, the modulation, the maximum packet length, the channel code, and many other design parameters may have been fixed. Given a signal-to-noise ratio, the data rate on a link, or its throughput, may be lower than the information capacity. Unless otherwise stated, when discussing “throughput” in the networking context, we assume that the system is designed to have low packet error rates so that packet errors can be ignored: this could be achieved by incorporating a sufficiently large power margin.

The remainder of this paper is organized as follows. Section 2 is a brief tutorial introducing the basic concept of PNC and overviewing various issues arising from PNC. Section 3 goes into the details of communication-theoretic studies of PNC. Results on asynchronous PNC and channel-coded PNC are discussed. Section 4 overviews some information-theoretic results of PNC and examines their implications. Section 5 considers MAC and network layer issues arising from PNC. In Section 6, we propose the idea of optical PNC. We conclude this paper in Section 7 by presenting some worthwhile future directions for PNC research.

2. A brief tutorial of PNC

The easiest way to illustrate the concept of PNC is through TWRC. TWRC is a three-node linear network in which two end nodes, nodes 1 and 2, want to communicate via a relay node R. There is no direct signal path between nodes 1 and 2. An example is a satellite network in which nodes 1 and 2 are the ground stations, and the relay R is the satellite.

The half-duplex constraint is often imposed on wireless communication systems to ease engineering design. With the half-duplex constraint, a node cannot transmit and receive at the same time. This means that the relay in TWRC cannot receive from node 1 or node 2 and transmit to them at the same time. A corollary is that each packet from node 1 to node 2 (and similarly, each packet from node 2 to node 1) must then use up at least two time slots to reach its destination. Thus, the best possible packet exchange throughput is two packets for every two time slots, one in each direction.

In the following, we examine the number of time slots needed for nodes 1 and 2 to exchange one packet with each other in various systems. In particular, we show that PNC can achieve the upper bound throughput of two packets every two time slots.

To proceed quickly to our discussion in a tutorial style, here we opt for a “bottom-up” approach in which notations are defined when they are first used. Readers who prefer a “top-down” approach are referred to the Appendix for the formal definitions of the TWRC system model and the collection of related notations. Throughout this paper, we use the uppercase letter to denote a packet and the corresponding lower-case letter to denote a symbol within the packet. For example, $S_1$ is a packet, and $s_1$ is a symbol within the packet.
at the symbol levels. The main difference between PNC and SNC is that PNC uses network coding whereas SNC does not. Although strictly speaking, many variants of PNC actually operate on the symbol level, even so using a network-coded packet simply as straightforward network coding (SNC).

2.2. Non-physical-layer network coding scheme (SNC)

A straightforward way of applying network coding can reduce the number of time slots to three [8,9]. We shall refer to this non-physical-layer network coding scheme simply as straightforward network coding (SNC). By reducing the number of time slots from four to three, SNC has a throughput improvement of 33% over TS.

Fig. 2 illustrates the idea of SNC. In time slot 1, node 1 transmits $S_1$ to relay $R$; in time slot 2, node 2 transmits $S_2$ to relay $R$. After receiving $S_1$ and $S_2$, relay $R$ forms a network-coded packet $S_R = f(S_1, S_2)$. General, many network-coding mappings $f(S_1, S_2)$ are possible. Various general forms will be discussed later in the paper. For simplicity, here we assume that packets $S_1$ and $S_2$ consists of QPSK symbols and that $f(S_1, S_2)$ is the XOR operation, as follows:

$$S_R = S_1 \oplus S_2$$

(1)

where $\oplus$ denotes the pairwise application of symbol-by-symbol XOR over $S_1$ and $S_2$. That is, if $S_1 = (a_1[1] + j b_1[1], \ldots, a_1[M] + j b_1[M]), S_2 = (a_2[1] + j b_2[1], \ldots, a_2[M] + j b_2[M]),$ then $S_R = ((a_1[1] \oplus a_2[1]) + j(b_1[1] \oplus b_2[1]), \ldots, (a_1[M] \oplus a_2[M]) + j(b_1[M] \oplus b_2[M])), \ldots$ while $M$ is the number of symbols in a packet. Note that for $n \times n$ QAM of a higher order than QPSK, we could interpret $S_1 \oplus S_2$ as $S_1 + S_2 (\mod n)$. Even this more generalized form of network-coding operation is only a subset of many possibilities.

In time slot 3, relay $R$ broadcasts $S_R$ to both nodes 1 and 2. When node 1 receives $S_R$, it extracts $S_2$ from $S_R$ using the self-information $S_1$ as follows:

$$S_1 \oplus S_R = S_1 \oplus (S_1 \oplus S_2) = S_2.$$  

(2)

Likewise, node 2 extracts $S_1$ from $S_2 \oplus S_R$.

Note that as with TS, SNC also tries to avoid simultaneous transmissions. That is, each node still transmits in a different time slot. Network coding is performed by the relay after receptions and decoding of the packets from nodes 1 and 2 in different time slots.

2.3. Physical-layer network coding scheme (PNC)

PNC further reduces the number of time slots to two. It allows nodes 1 and 2 to transmit together and exploits the network coding operation performed by nature in the superimposed EM waves. By doing so, PNC can improve the performance of TS by 100%.

Fig. 3 illustrates the idea. In the first time slot, nodes 1 and 2 transmit $S_1$ and $S_2$ simultaneously to relay $R$. Based on the superimposed EM waves that carry $S_1$ and $S_2$, relay $R$ deduces $S_R = S_1 \oplus S_2$. Then, in the second time slot, relay $R$ broadcasts $S_R$ to nodes 1 and 2.

A key issue in PNC is how relay $R$ deduces $S_R$ from the superimposed EM waves. We refer to this process as “PNC mapping”. More generally, PNC mapping refers to the process of mapping the received superimposed EM waves plus noise to some output packet for forwarding by the relay. PNC mapping could output a packet in a different form than $S_1 \oplus S_2$. Section 2.4 will discuss other possibilities for $S_R$. All PNC mappings share the key requirement that nodes 1 and 2 must be able to deduce $S_1$ and $S_2$, respectively, based on $S_R$ and self-information $S_1$ and $S_2$, respectively.

For the discussion in this section, let us assume the PNC mapping $S_R = S_1 \oplus S_2$ and QPSK modulation. We further assume symbol-level and carrier-phase synchronization, and the use of power control, so that the packets from nodes 1 and 2 arrive at relay $R$ with the same phase and amplitude. We ignore noise in our simplified presentation for the time being.

Consider one particular symbol period. Suppose that nodes 1 and 2 modulate their symbols on RF frequency $\omega$. The signal sent out by node $i$ is $Re(a_i + j b_i e^{j\omega t})$. The combined bandpass signal received by relay $R$ during one symbol period is

$$y_R(t) = s_1(t) + s_2(t)$$

$$= [a_1 \cos(\omega t) - b_1 \sin(\omega t)] + [a_2 \cos(\omega t) - b_2 \sin(\omega t)]$$

$$= (a_1 + a_2) \cos(\omega t) - (b_1 + b_2) \sin(\omega t)$$

(3)
where $s_i(t), i \in \{1, 2\}$, is the bandpass signal transmitted by node $i$; and $a_i \in \{-1, 1\}$ and $b_i \in \{-1, 1\}$ are the corresponding QPSK modulated information bits. For QPSK, $a_i = 1$ corresponds to bit 0, and $a_i = -1$ corresponds to bit 1; likewise for $b_i$. With this definition, XOR becomes arithmetic multiplication: i.e., $a_1 \oplus a_2 = a_1 a_2$ and $b_1 \oplus b_2 = b_1 b_2$.

The baseband in-phase ($I$) and quadrature ($Q$) components corresponding to (3) are

$$y_R^{(I)} = a_1 + a_2$$
$$y_R^{(Q)} = b_1 + b_2.$$  

Note that relay $R$ cannot extract the individual symbols transmitted by nodes 1 and 2 from (4). This is because $y_R^{(I)}$ and $y_R^{(Q)}$ in (4) gives us two equations, but there are four unknowns: $a_1, b_1, a_2$, and $b_2$.

In PNC, however, relay $R$ does not need the individual values of the four unknowns; it only needs to derive the two values, $a_1 \oplus a_2$ and $b_1 \oplus b_2$, to produce the PNC mapping $S_R = a_1 a_2$, $b_1 b_2$. In particular, $a_1 \oplus a_2$ and $b_1 \oplus b_2$ can be derived from $y_R^{(I)}$ and $y_R^{(Q)}$, respectively. That is, we can find a PNC mapping function $f(\cdot, \cdot)$ such that $S_R = f(y_R^{(I)}, y_R^{(Q)})$.

Table 1 shows the PNC mapping for the in-phase component $a_R$; the mapping for the quadrature component $b_R$ is similar. For QPSK, $a_R = a_1 a_2 = -1$ if $a_1 \neq a_2$, and $a_R = a_1 a_2 = 1$ if $a_1 = a_2$. There are three possible values for $y_R^{(I)} = a_1 + a_2$: 0, 2, and −2. Since $y_R^{(Q)} = 0$ when $a_1 \neq a_2$, and $y_R^{(I)} = -2$ or 2 when $a_1 = a_2$, the PNC mapping is as follows:

$$a_R = \begin{cases} -1 & \text{if } y_R^{(I)} = 0 \\ 1 & \text{if } y_R^{(I)} = -2 \text{ or } 2. \end{cases}$$  

After the PNC mapping, relay $R$ transmits the following signal to nodes 1 and 2 in time slot 2:

$$s_R(t) = a_R \cos(\omega t) - b_R \sin(\omega t).$$  

The RF signal transmitted in time slot 2 in PNC is the same as the RF signal transmitted in time slot 3 in SNC. The key difference of the two systems lies in how they derive $(a_R, b_R)$. In SNC, $(a_1, b_1)$ and $(a_2, b_2)$ are separately transmitted by nodes 1 and 2; and relay $R$ explicitly decodes $(a_1, b_1)$ and $(a_2, b_2)$ in order to form $(a_R, b_R)$. In PNC, $(a_R, b_R)$ is derived from $(a_1 + a_2, b_1 + b_2)$, which is the superimposed signal in time slot 1.

Table 1

| Symbol from node 1: | Symbol from node 2: | Composite symbol received at relay $R$: $y_R^{(i)} = a_1 + a_2$ | Mapping to symbol to be transmitted by relay $R$: $a_R$ |
|---------------------|---------------------|-------------------------------------------------|-----------------|
| 1                   | 1                   | 2                                               | 1               |
| −1                  | −1                  | 0                                               | −1              |
| 1                   | −1                  | −2                                              | 1               |

We remark that the arithmetic sums in $(a_1 + a_2, b_1 + b_2)$ is also a form of network coding operation. In particular, it is the network coding performed by nature. In the above example, the relay transforms it to the XOR network coding operation $(a_1 \oplus a_2, b_1 \oplus b_2)$. In general, among many other possibilities, the relay could also retain $(a_1 + a_2, b_1 + b_2)$ as the PNC mapping to be used.

2.4. Generalization of PNC

So far, we have assumed the desired network-coded signal is the XOR of the signals from nodes 1 and 2. As already mentioned, in general, PNC mapping is not limited to just the XOR mapping.

In the broadest scope of PNC, the goal of the relay is to map the input signals simultaneously received from many transmitters to a network-coding function: $S_R = f(S_1, S_2, \ldots)$ where $S_1, S_2, \ldots$ are the messages from these transmitters, and $S_R$ is the target network-coded message to map to. In TWRC, there are only two messages $S_1$ and $S_2$ from two transmitters, and the relay will broadcast $S_R$ back to nodes 1 and 2 after this mapping. The key idea is that nodes 1 and 2 should be able to derive their counterparts’ messages from $S_R$ and self-information. That is, there must be a network-decoding function $g$ such that $S_R = g(f(S_1, S_2), S_I)$ where node 1 can extract the information from node 2 upon receiving $S_R$. In general, many forms of the network-coding-decoding function pairs, $(f, g)$, are possible. It is the exploitation of such function pairs in information delivery that distinguishes network-coding relay systems from traditional non-network-coding relay systems.

According to whether the range of $f$ is a finite or infinite set, Zhang et al. [10] classifies PNC mappings at the relay into two categories: finite-set PNC (abbreviated as PNCF) and infinite-set PNC (abbreviated as PNCI).

Examples of PNCF include the PNC mapping discussed so far and the simple extension of it to $n \times n$ QAM in which $\oplus$ is interpreted as mod $n$ addition. Refs. [11, 12] showed that even when both nodes 1 and 2 use QPSK modulation, when the phases of the RF signals from the two end nodes are not exactly aligned, it is sometimes more desirable for the relay $R$ to use 5QAM (as opposed to QPSK) for the signal it transmits to nodes 1 and 2. In this case, the range of $f$ for each symbol is a finite set consisting of five elements. The use of structured codes such as the nested lattice code in the compute-and-forward framework [13] and in [14] are other examples of PNCF.

Examples of PNCl include the Analog Network Coding (ANC) in [6,7]. In ANC, the relay retains the additive mixing that occurs in nature and simply amplifies the simultaneously received signals (plus noise) and forwards it to the two end nodes. The operation is done on a symbol-by-symbol basis. For symbols $S_1$ and $S_2$, the target output symbol is $S_R = f(S_1, S_2) = h_{1R}S_1 + h_{2R}S_2$ where $h_{1R}$ and $h_{2R}$ are the channel gains of nodes 1 and 2 to the relay, respectively. In this case $h_{1R}$ and $h_{2R}$ are complex and the range of $f$ is an infinite set in general.

Loosely speaking, PNCF aims to produce a discrete output at the relay while PNCl aims to produce an analog output through a functional mapping $f$. A subtlety is that...
this does not mean the relay will necessarily just send out \( f \) as is. For example, for symbol-by-symbol XOR mapping in which \( s_k = f(s_{1}, s_{2}) = s_{1} \oplus s_{2} \), we could perform an MMSE (minimum mean-square error) estimate of \( s_{1} \oplus s_{2} \) and send out the MMSE. In this case, even though we are dealing with PNCF in which \( s_{1} \oplus s_{2} \) is discrete, the MMSE is in the analog form. By PNCF, we mean that the range of \( f \) itself is discrete and the arguments of the function \( g(f(s_{1}, s_{2}), s_{1}) \) are discrete.

Conversely, for PNCI, the relay does not necessarily send out an analog message. The PNC scheme operated with compress-and-forward [15], for example, quantizes the analog output from ANC and channel-codes the quantized information before forwarding the signal. Although \( f \) is analog, the processed information after quantization and channel coding is discrete.

In Sections 3.1.1 and 3.1.2, we will further discuss various schemes of finite- and infinite-field PNC.

2.5. Important issues in PNC

To ease exposition, we have ignored many important issues so far. This section gives an overview of these issues.

2.5.1. Consideration of noise

Fundamental to all communication systems is the presence of noise. In our discussion thus far, we have ignored noise. Our throughput analysis has been based on time slot counting, assuming whatever is sent will be received correctly. A more in-depth analysis must include the consideration of noise. With noise, (4) becomes

\[
y_R = a_1 + jb_1 + a_2 + jb_2 + w_R
\]

where \( w_R \) is the noise typically modeled as a Gaussian random variable.

With noise, an issue in XOR PNC mapping, for example, is whether the bit error rate (BER) will increase relative to that in TS or SNC. It turns out that with QPSK modulation, the “end-to-end BER” between nodes 1 and 2 of PNC is comparable to that of TS, and is actually slightly better than that of SNC, as explained in the next three paragraphs.

Let \( P_e \) be the BER of the classical QPSK point-to-point link. Thus, TS consists of four such one-hop links. In the TS, SNC, and PNC discussed below, for simplicity, let us assume equal transmit power for all nodes, equal channel gain in all directions, and equal receiver noise power at all nodes. Then, \( P_e \) is the same for all the one-hop links in TS. The end-to-end BER of TS is therefore \( 2(1 - P_e)P_e \). That is, a transmitted bit is in error under two situations: (i) there is a detection error in the first hop, but no detection error in the second hop; or (ii) there is no detection error in the first hop, but there is a detection error in the second hop.

The BER of the classical QPSK point-to-point link \( P_e \) is plotted in Fig. 4. For comparison the BER of \( a_k \) (or \( b_k \)) in the uplink of the XOR PNC system is also plotted in Fig. 4. We refer the interested reader to [1] for the derivation of the BER of \( a_k \) and \( b_k \). Recall that for PNC and SNC, the target signal at the relay is the XOR signal; thus, the BER is the BER of the decoded XOR, not the BER of the individual bits from the two ends. We note from Fig. 4 that the uplink BER of \( a_k \) (or \( b_k \)) in PNC is roughly the same as the BER of a point-to-point QPSK link, \( P_e \). Therefore, using the same argument as in the previous paragraph, the end-to-end BER of PNC is approximately \( 2(1 - P_e)P_e \), the same as in TS. Note, however, that PNC uses two time slots and TS uses four time slots. Thus, at equal BER, the throughput of PNC is twice that of TS.

For SNC, the BER of \( a_k \) (or \( b_k \)) at the relay is \( 2(1 - P_e)P_e \). That is, there is an XOR decoding error if the bit from node 1 is decoded with error and the bit from node 2 is decoded correctly, and vice versa. Thus, the uplink BER of SNC (also plotted in Fig. 4) is equal to the end-to-end BER of TS and PNC. The end-to-end BER of SNC is \( 2(1 - P_e)P_e \cdot (1 - P_e) + [1 - 2(1 - P_e)P_e] \cdot P_e = 3P_e - 6P_e^2 + 4P_e^3 > 2(1 - P_e)P_e \) for \( P_e > 0 \). We see that SNC not only have smaller throughput than PNC, it also has higher BER.

Automatic Repeat reQuest (ARQ)

The above analysis has assumed no error control. For reliable communication, ARQ can be used in each hop. In this case, CRC bits (cyclic redundancy check bits) are added to the data packets. When errors are detected, the transmitter will be requested to retransmit the packet. In the following, we briefly discuss the throughputs of TS, SNC, and PNC when ARQ is incorporated.

Suppose that there are \( N \) bits in a packet (including the CRC bits) and that bit errors are independent. The packet error probability is \( P_e = 1 - (1 - P_e)^N \). We assume that packet errors of different packets are i.i.d. For simplicity, we also assume that error detection is perfect, i.e., all errors can be detected. We define one time slot as the time needed for a node to transmit one data packet plus the time needed to determine whether the packet has been received correctly (through acknowledgments from the receiver(s) or other mechanisms). Throughput is defined as the average number of packets that can be transferred successfully from node 1 to node 2, and vice versa, per time slot. That is, throughput is a normalized quantity upper-bounded by 1 here.

For TS, four hops are required to deliver two packets. Under the i.i.d. assumption, the time needed for each hop with ARQ is a geometric distribution with mean \( 1/(1 - P_e) \). Thus, four hops require \( 4/(1 - P_e) \) time units on average. The throughput is therefore \( TH_{TS} = (1 - P_e)/2 \).

For SNC, the two uplink hops consume \( 2/(1 - P_e) \) time slots on average. The downlink hop broadcasts the
same information to the two end nodes. After the first transmission, it is possible that both end nodes receive the packet successfully, only one of them receives it successfully, or none of them does. A Markov chain can be set up for the overall process. Let $T_0$ be the average time needed for the downlink hop. Let $T_1$ be the average remaining time needed for the downlink hop after one of the nodes has received the packet successfully. By renewal argument, it is easy to see that $T_0 = 1 + \tilde{P}_2^2 T_0 + 2 \tilde{P}_2 (1 - \tilde{P}_2) T_1$ and $T_1 = 1 + \tilde{P}_2 T_1$. Solving the equations yields $T_0 = (1 + 2 \tilde{P}_2)/(1 - \tilde{P}_2^2)$. Thus, $Th_{SNC} = 2/(2/(1 - \tilde{P}_2) + T_0) = 2(1 - \tilde{P}_2^2)/(3 + 4 \tilde{P}_2)$.

For PNC, the uplink time is $1/(1 - \tilde{P}_2)$ on average. The downlink time is $T_0$ on average, as in SNC. Therefore, $Th_{PNC} = 2/(1/(1 - \tilde{P}_2) + T_0) = 2(1 - \tilde{P}_2^2)/(2 + 3 \tilde{P}_2)$.

Based on the above results, it is easy to show that $Th_{PNC} \geq Th_{SNC} \geq Th_{TS}$. In particular, in the high SNR regime with $\tilde{P}_2 \to 0$, we have $Th_{PNC} = 1$, $Th_{SNC} = 2/3$, and $Th_{TS} = 1/2$, as validated by our earlier slot counting exercise that ignored noise. Thus, at the high SNR regime, the improvements of PNC over SNR and TS are 50% and 100%, respectively.

In the low SNR regime, the performance advantage of the network coded schemes over the traditional scheme is less distinct. For example, $\lim_{\tilde{P}_2 \to 0} Th_{PNC}/Th_{SNC} = 7/5$ and $\lim_{\tilde{P}_2 \to 0} Th_{PNC}/Th_{SNC} = 8/5$: the performance improvements of PNC over SNC and TS are reduced to 40% and 60%, respectively. Instead of ARQ, the use of channel coding for forward error control may maintain the near 100% gain of PNC over TS in the low SNR regime as well as the high SNR regime. This is indicated by our information-theoretic discussion in Section 4 (see Fig. 21, Table 3 and the discussion thereof).

Our discussion above has focused on XOR PNC mapping. In general, investigations of other finite- and infinite-field PNC schemes [10] should also take into the consideration of noise, especially when comparing their relative performance.

2.5.2. Forward error control with channel coding

In the previous section, we have briefly discussed the use of ARQ for error control. An alternative is to use forward error control. In a communication system with noise, the use of channel coding for forward error control is an important technique to ensure reliable transmission.

With channel coding, nodes 1 and 2 in the PNC system map their source packets $S_1$ and $S_2$ to channel-coded packets $C_1$ and $C_2$, respectively. An issue in PNC is how to integrate channel coding into the system. In general, channel coding can be applied on a link-by-link basis or on an end-to-end basis. In the former, the relay performs channel decoding and re-encoding in addition to PNC mapping. In the latter, the relay only performs non-channel-coded PNC mapping, and only the source performs channel coding and only the end receiver performs channel decoding.

In end-to-end channel-coded PNC, at the destination node, say node 1, after the channel-coded self-information $C_1$ is removed from the received signal, the remaining signal is just the channel-coded signal $C_2$ plus noise. The channel decoding operation at the end node is much like that in a traditional point-to-point communication system. Because the relay does not clean up the relay noise by channel decoding and re-encoding, noise can accumulate from hop to hop. The noise accumulation can become severe in a more general setting in which there are many relays in between the two end nodes.

In link-by-link channel-coded PNC, channel decoding at the relay can be tricky (as compared to channel coding in an ordinary point-to-point communication link). This is because the ultimate goal at the relay is to recover $S_1 \oplus S_2$ (or a general network-coded form $f(S_1, S_2)$), not the individual source information $S_1$ and $S_2$. After obtaining $S_1 \oplus S_2$, the relay can then channel-code $S_1 \oplus S_2$ before transmitting the channel-coded packet to the two end nodes. The two-step process is performed so as to clean up the noise before information forwarding. A subtlety of the first step $Y_R \rightarrow S_1 \oplus S_2$ is as follows. Note that $Y_R$ contains the arithmetic superposition of $C_1$ and $C_2$, not the arithmetic superposition of $S_1$ and $S_2$. In particular, the mapping $Y_R \rightarrow S_1 \oplus S_2$ involves both channel decoding and PNC mapping operations in that instead of channel decoding to obtain $S_1$ and $S_2$, we want to channel decode to obtain $S_1 \oplus S_2$. Different ways of integrating such channel-decoding and PNC mapping at the relay may lead to different performance. For example, we could still first channel decode to obtain $S_1$ and $S_2$ individually and compute $S_1 \oplus S_2$ after that. This turns out to work well in the low SNR regime, but not the high SNR regime. Section 3.2 will discuss several schemes and delves into the relevant issues.

2.5.3. Synchronization

The discussion of PNC thus far assumes perfect synchronization between nodes 1 and 2, so that their packets arrive at the relay with the packet boundary and symbol boundary aligned. In addition, the RF frequencies used by the two nodes are the same, and their relative phase offset is zero. Indeed, the discussion of PNC in [1] was heavily focused on the perfectly synchronized case. An issue is whether there will be performance degradations (and if so, their extents) when PNC does not operate with such perfect synchronization.

Synchronization can be separated into different time scales. First, the packets simultaneously transmitted by the two end nodes may not arrive at the relay perfectly aligned. Packet alignment is a MAC-layer scheduling issue. Compared with other types of synchronization, longer time scale is involved. MAC layer methods could be introduced to synchronize the transmissions of packets by nodes 1 and 2.

However, even if nodes 1 and 2 transmit their packets simultaneously, it is possible for the packets to arrive at the relay with their symbol boundaries unaligned. Thus, a symbol from one node may overlap with two symbols from the other nodes. Symbol alignment is at a finer time scale than packet alignment and is therefore more challenging. There have been studies on how to align symbols of different transmitters at a common receiver [16]. This is a fundamental issue of relevance to many communication systems, not just PNC.
Even if symbols from the two nodes could be aligned, there would still be the issue of RF carrier frequency synchronization and relative phase offset. If the RF carrier frequencies at nodes 1 and 2 are derived from a common source, then there will be no frequency offset. If not, the frequency offset translates into a rotating phase offset: that is, the relative phase offset between the two nodes varies from symbol to symbol in a packet. In general, for a particular pair of symbols from the two end nodes, the baseband components in (7) become

\[ y_R = a_1 + jb_1 + (a_2 + jb_2)e^{j\phi} + w_R \]  

(8)

where \( \phi \) is the relative phase offset between the pair of symbols. Phase offset \( \phi \) is independent of time and is the same for all symbols in the packet if the RF frequencies of the two nodes are exactly the same; otherwise, \( \phi \) will change incrementally in successive symbol pairs.

Recall that we want to estimate both \( a_1 \oplus a_2 \) and \( b_1 \oplus b_2 \) based on the signal reception \( y_R \) in (8). With the phase asynchrony as in (8), for optimal performance, we cannot just separate out the real and imaginary components of \( y_R \) and process them separately to obtain the estimates of \( a_1 \oplus a_2 \) and \( b_1 \oplus b_2 \). With QPSK, there are 16 constellation points based on different combinations of \( (a_1, b_1, a_2, b_2) \). These 16 points are in turn mapped to the four constellation points of \( (a_1 \oplus a_2, b_1 \oplus b_2) \).

The BER of \( a_1 \oplus a_2 \) and \( b_1 \oplus b_2 \) will depend on the phase offset \( \phi \). For QPSK, \( \phi = \pi/4 \) has the worst BER while \( \phi = 0 \) has the best BER. Beyond \( \phi = \pi/4 \), the desired map will be \( (a_1 \oplus b_2, b_1 \oplus b_2) \) rather than \( (a_1 \oplus a_2, b_1 \oplus b_2) \) and the BER will decrease from \( \phi = \pi/4 \) to \( \phi = \pi/2 \). These results are summarized in Fig. 9 and elaborated in Section 3.

Synchronization issues in PNC have drawn the attention of researchers since it was conceived. In the accompanying technical report to [1] (http://arxiv.org/abs/0704.2475), signal detection in the presence of asynchrony was discussed in its Appendix 2. The detection method is suboptimal and gives up useful signal energy. In [17], it was pointed out in PNC systems operated with QPSK modulation, there is a significantly power penalty of 6 dB when the carrier phases of the two end nodes are not synchronized and offset by \( \pi/4 \), calling into question the viability of PNC in the lack of synchronization. Ref. [18], however, shows that the phase penalty goes away in channel-coded PNC, and for QPSK, the penalty due to phase asynchrony can actually be turned into a reward with channel coding. Asynchronous PNC is current one of the very active areas in PNC research. This section only quickly runs through the underlying issues. Much space of Section 3 of this paper is devoted to the discussion on the synchronization issues at a deeper level.

2.5.4. Non-symmetric fading channels and channel estimation

The discussion thus far assumes that the channels are symmetric. In general, nodes 1 and 2 can be at different distances from the relay. Also, the channels may undergo fading. Let \( h_i \) be the complex number denoting the channel gain for the uplink channel from node \( i \) to relay \( R \). For flat fading over the RF bandwidth of concern, the sampled symbol at the relay is

\[ y_R = h_{1R}(a_1 + jb_1) + h_{2R}(a_2 + jb_2) + w_R. \]

(9)

The relay must estimate \( h_{1R} \) and \( h_{2R} \) in order to perform detection effectively. This estimation is typically done via known training symbols and/or pilots embedded in the packets. Channel estimation in PNC systems has also been an active area of research because unlike the point-to-point communication system in which only one channel gain needs to be estimated, two channel gains need to be estimated based on the simultaneously received signals.

If nodes 1 and 2 know \( h_{1R} \) and \( h_{2R} \) (say via feedback from the relay which estimates \( h_{1R} \) and \( h_{2R} \)), they could multiply the symbol \( (a_1 + jb_1) \) by \( h_{1R}/|h_{1R}|^2 \) and the symbol \( (a_2 + jb_2) \) by \( h_{2R}^*/|h_{2R}|^2 \), respectively, before transmitting them. Doing so will yield the same equation as (7) for the received signal at the relay. In TWRC, for example, each time the relay broadcasts a packet to nodes 1 and 2, it could also embed \( h_{1R} \) and \( h_{2R} \) estimated by it within the broadcast packet. This way, nodes 1 and 2 can use this information to precode the symbols in the next packet transmitted to the relay. Generally, transmitter precoding by nodes 1 and 2 can lead to better performance.

There are two scenarios under which transmitter precoding is impractical. The first is the fast fading case in which the channel gains vary quickly so that between the transmission of one packet and the next, \( h_i \) has already changed substantially. The feedback \( h_i \) from relay \( R \) to node \( i \) is therefore not reflective of the actual \( h_i \) in the next time slot. The second is the bursty, sporadic traffic case in which the end nodes do not always have packets to transmit, and the relay is shared by many pairs of end nodes. In this case, a random access MAC protocol may be used to coordinate the packet exchange between the different node pairs. The intervening time between two successive packet exchange of a particular node pair may be long, and that \( h_i \) may have changed significantly since the last exchange.

In general, systems in which transmitter precoding is not used are simpler to implement and are applicable to a wider range of scenarios. For this reason, most research on PNC has assumed the end nodes do not precode. Note that precoding by the relay is a different story. If the channels are symmetric so that \( h_{Ri} = h_{Ri} \), the relay could use its knowledge on \( h_{IR} \) (which has to be estimated anyway) to precode the signal it relays to the end nodes. Relaying occurs almost immediately after the transmission by nodes 1 and 2: therefore, if the channel gains do not change drastically from time slot to time slot, this strategy is still valid.

For non-flat fading over the transmission bandwidth, (9) is not valid and there will be inter-symbol interference. OFDM is a powerful technique for dealing with non-flat fading. The basic idea of OFDM is to carry the symbols on multiple sub-bands. If the sub-bands are narrow enough, the fading in each sub-band is flat. Thus, on each sub-band, (9) remains valid. In addition, OFDM provides a natural way to deal with the relative symbol offset between nodes 1 and 2 in PNC. In particular, any time-domain symbol offset will be translated to a phase term in the channel.
2.5.5. Information-theoretic analysis

At the most fundamental level, the performance of PNC should be analyzed from an information-theoretic perspective. This study falls into the domain of network information theory [19]. For TRWC, for example, of concern is the information exchange rates that can be achieved from node 1 to node 2, \( R_{12} \), and from node 2 to node 1, \( R_{21} \), subject to the noise.

It has been found that finite-field mapping schemes can achieve near information-capacity rates [20], whereas infinite-field mapping schemes such as ANC [6] cannot. In [14], it was shown that under Gaussian-noise channels, finite-field PNC with the use of lattice code can achieve rates within 1/2 bit of the cut-set outer bound in TRWC.

In general, link-by-link channel-coded schemes have better exchange-rate performance than end-to-end channel-coded schemes. Within the category of link-by-link channel coded schemes, the relative performance of different schemes depend on the SNR regime of operation.

In TWRC, the rates \( R_{12} \) and \( R_{21} \) could be uplink-limited (limited by the links from nodes 1 and 2 to relay \( R \)), downlink-limited (limited by the links from relay \( R \) to nodes 1 and 2), or both uplink-and-downlink limited. Section 4 will present a detailed discussion of TWRC from an information-theoretic perspective.

2.5.6. General network topologies and higher-layer issues

The original proposal of PNC in [1] gave a brief discussion of its application in networks of general topologies, and the implications of PNC for higher-layer issues such as MAC scheduling and routing. The majority of the subsequent PNC investigations, however, focused on TWRC.

It is straightforward to extend the TWRC scenario to a linear network scenario in which two end nodes exchange information via a chain of relays between them. With proper scheduling, as illustrated in Fig. 5 (see [1] for a more detailed description), the exchange throughput of 1/2 packet per direction per time slot can be achieved (i.e., same as in TWRC).

For a general multihop network, there could be many end-to-end flows. Each flow is between two end nodes, and the intermediate nodes between the two nodes serve as the relays for the flow. If the flow is bidirectional and there are equal amounts of traffic in the two directions, then the bidirectional flow could make use of PNC. The two end nodes and the intermediate nodes traversed by the bidirectional flow look like the linear network in Fig. 5. A difference in a general network, however, is that the relay nodes may not be dedicated to that bidirectional flow alone. There could be many flows traversing a node, and therefore the transmission time of a node may need to be divided among the multiple flows. Thus, in addition to the intra-flow scheduling such as that shown in Fig. 5, the inter-flow scheduling also needs to be considered.

PNC matches best with the bidirectional setting with equal amounts of traffic in opposing directions. However, in a network supporting general applications, we could also have unidirectional end-to-end flows. In addition, for some applications with bidirectional flows, the amounts of traffic in the two directions may not be equal. An example is a TCP file download session in which the TCP DATA mainly flows from the file server to the client, and there is relatively little traffic of TCP ACK in the other direction.

The concept of virtual path can be applied to the general setting. We could establish many balanced-traffic bidirectional virtual paths to exploit PNC in the optimal way. Each balanced-traffic bidirectional virtual path is a linear PNC chain similar to that in Fig. 5. We could aggregate the traffic from multiple end-to-end flows onto each bidirectional virtual path. An example is shown in Fig. 6, in which we show the aggregation of two unidirectional flows. The overlapped portions of the two unidirectional flows could be carried on a bidirectional PNC virtual path. The non-overlapped portions could aggregate with other flows on other bidirectional PNC virtual paths.

In general, each end-to-end flow may traverse a sequence of bidirectional virtual paths. The end-to-end flow may be aggregated with different flows on different bidirectional virtual paths in the sequence. Also, in general, each bidirectional virtual path may aggregate the traffic from many flows (i.e., more than the two flows as shown in the simple example of Fig. 6). In particular, a bidirectional virtual path may aggregate the traffic from different flows in such a way that the aggregated traffic volumes in both directions of the virtual path are approximately equal, so that optimal use of PNC can be attained. Thus, the general
principle is that for each unit of traffic in one direction, we try to find a unit of traffic (possibly from another flow) in the opposite direction for aggregation purposes.

Despite the best attempt, there could still be some remainder traffic in one direction that cannot be matched to traffic in the opposite direction. Thus, in addition to the bidirectional PNC virtual paths, the network could also form unidirectional virtual paths to carry such unmatched traffic. The unidirectional virtual paths could either use the traditional multihop method to schedule packet transmission along the path, or they could use unidirectional PNC scheduling. We refer the interested reader to [1] for details on unidirectional PNC, which in general could be more efficient than traditional unidirectional multihop scheduling.

In wired networks, the virtual paths that do not overlap do not mutually interfere. In wireless networks, non-overlapping virtual paths may still mutually interfere when their nodes are within the proximity of each other. Thus, unlike in wired networks, nearby virtual paths in wireless networks are not decoupled, and the scheduling of the transmission times of the nodes in a virtual paths must take into account the transmission times of the nodes in nearby virtual paths.

Besides scheduling, there is also the routing issue when deciding the route for an end-to-end flow. With the virtual path concept above, however, the problem becomes finding a sequence of virtual paths with enough unused capacity to carry the flow. To our best knowledge, the above virtual path framework in the context of PNC has not been carefully studied so far and is first proposed here in this article. More generally, how to decompose the general problem of scheduling and routing in large-scale networks when PNC is applied is still an open issue.

2.6. Concluding remarks for the brief tutorial

We have given a quick introduction to PNC and the issues involved. In the remaining sections, we will go into some of these issues at a deeper level. We conclude this brief tutorial by making some general observations about the status of PNC research to-date.

Among the three areas of PNC research (i.e., communication-theoretic, information-theoretic, and networking), networking issues have received the least attention today. Yet networking issues will become important when we extend the application of PNC beyond TWRC. As the theoretical understanding of PNC in TWRC matures, we anticipate future research focus will move toward the application of PNC in general topologies, with network and MAC-scheduling issues taking increasing important roles.

In addition, there have been little implementation and prototyping efforts for PNC. To our best knowledge, Katti et al. [6] was the first work that prototyped a PNC system. The simple amplify-and-forward TWRC system was chosen for implementation in [6]. This was followed by a gap of several years before an XOR PNC system was implemented in [22]. An implementation in the frequency domain based on OFDM was chosen in [22] to obviate the need for tight synchronization. We are not aware of other PNC implementation efforts besides [6,22]. As the theoretical understanding of PNC matures, the implementation arena is likely to become a fertile ground for future research.

3. Communication-theoretic studies

In this section we delve into the communication-theoretic studies of PNC, focusing on TWRC. We start with non-channel-coded PNC in Section 3.1. Section 3.2 discusses channel-coded PNC. In particular, we discuss various ways in which channel coding can be integrated into the PNC framework. In both Sections 3.1 and 3.2, we will examine the synchronization issue.

3.1. Non-channel-coded PNC

In [1], the XOR PNC mapping was explored. Since then, many other schemes have been investigated. In general, these schemes can be divided to two categories according to the PNC mapping involved: PNC over finite set (PNCF) and PNC over infinite set (PNCI) [10].

Assume symbol alignment for the time being. Let \( (x_1[n], x_2[n]) \), \( 1 \leq n \leq N \), be a pair of symbols from nodes 1 and 2 that are received at the same time at relay \( R \). For simplicity, we will omit the index \( n \) in our notation below when no confusion will arise. For non-channel coded systems, \( (x_1, x_2) = (s_1, s_2) \), the pair of source symbols. The signal received by relay \( R \) is

\[
y_R = h_{1R}x_1 + h_{2R}x_2 + w_R
\]

where \( h_{1R} \) is the channel gain from node \( i \) to relay \( R \), and \( w_R \) is the Gaussian noise. We assume the transmit power has been factored into the \( h_{1R} \). That is, \( h_{1R} = \sqrt{P_i^f g_{IR}} \), where \( P_i^f \) is the transmit power, and \( g_{IR} \) is the actual gain of the channel.

The relay attempts to map \( y_R \) to a target network-coded symbol \( z_R = f(x_1, x_2) \) for broadcast back to nodes 1 and 2. In PNCF, \( z_R \) is a symbol chosen from a finite set, and there are only a finite number of possibilities for \( z_R \). For example, in XOR PNC mapping [1] the target symbol is

\[
f(x_1, x_2) = x_1 \oplus x_2
\]

where \( \oplus \) is the XOR operation.
$z_R = x_1 \oplus x_2$, and therefore XOR PNC belongs to PNCF. In PNCI, $z_R$ is a symbol chosen from an infinite set. For example, in amplify-and-forward PNC, i.e., ANC in [6], $z_R = h_1 x_1 + h_2 x_2$. Since $z_R$ is a complex number, ANC belongs to PNCI. Table 2 lists other examples of PNCF and PNCI.

Because of noise, the relay can only get an estimate for $z_R$, denoted as $\hat{z}_R$. Note that while $z_R$ is a function of $(x_1, x_2)$, $\hat{z}_R$ is a function of $y_R$. It is the estimate $\hat{z}_R$ that is actually sent by the relay. That is, the relay sends $x_R = \hat{z}_R$ to nodes 1 and 2. As will be further explained, although in PNCF $z_R$ is drawn from a finite set, the corresponding $\hat{z}_R$ can be drawn from an infinite set; similarly, although in PNCI $z_R$ is drawn from an infinite set, the corresponding $\hat{z}_R$ can be a quantized version of $z_R$ drawn from a finite set.

### 3.1.1. PNCF

In [1], the simplest PNCF scheme was considered. The constellations of $x_1$, $x_2$, and $z_R$ are all QPSK constellation. The QPSK–QPSK PNC mapping has good performance when $h_{1R}/h_{2R} = 1$, and this was the case assumed in our earlier presentation of PNC in Section 2.3.

When the relative phase offset of the signals from the two nodes is $\pi/4$, so that $h_{1R}/h_{2R} = e^{j\pi/4}$, there will be a significant performance penalty. Ref. [17] mentioned (without providing a proof) that the penalty could be as high as 6 dB. It turns out that for BER of 10$^{-2}$, the penalty is already 6 dB. For lower BER, the penalty is even higher (see Fig. 9(a), which will be elaborated later). This observation is quite alarming, and raises a question as to whether PNCF is viable in practice when the system is asynchronous. In Section 3.1.3, however, we will present results showing that this penalty can be significantly reduced when the symbols from the two end nodes arrive at the relay misaligned. Also, in Section 3.2.2, we will present results showing that the phase penalty in non-channel-coded PNC becomes a “phase reward” in channel-coded PNC. This leads us to believe that phase asynchrony is not a fundamental performance-limiting factor.

Ref. [11] showed that for QPSK $x_1$ and $x_2$, it is not always best to have QPSK $z_R$. The symbol-aligned case was studied. In particular, it was shown that when $h_{1R}/h_{2R} = 1$, a constellation map with at least five constellation points (e.g., 5QAM) for $z_R$ is needed in order that the end nodes can decode the symbol from the other node, even in the absence of noise. When the symbols are misaligned and/or when channel coding is incorporated into the PNC system, certain diversity and certainty propagation effects will cause phase asynchrony to be a lot less detrimental (more on this in Sections 3.1.3 and 3.2.2) in QPSK–QPSK mapping. Thus, it is not clear that in a practical system, QPSK–5QAM mapping is necessary, especially in view of the fact that this will complicate the implementation of channel-coded PNC.

In our discussion of PNCF thus far, we treat $z_R$ as the target mapped symbol, and assume the decoding of the composite signal at $R$ is such that the estimate $\hat{z}_R$ is also drawn from the same set as $z_R$. That is, both $z_R$ and $\hat{z}_R$ are elements belonging to the same finite set $F$. In estimation theory, even if the target $z_R \in F$, it is possible that $\hat{z}_R \notin F$ and that $\hat{z}_R$ is drawn from an infinite set. Refs. [10,23] discussed a number of such possibilities in detail. For example, in XOR PNC mapping with BPSK, $z_R = x_1 \oplus x_2, x_1, x_2, z_R \in \{-1, 1\}$, but the MMSE estimate of $z_R$ is a real number. Thus, when MMSE estimate is adopted, the relay actually sends out an analog rather than a discrete signal.

For MMSE, the relay transmits $x_R = \hat{z}_R = E[z_R|y_R] = P(z_R = 1|y_R) - P(z_R = -1|y_R)$, from which we can see that the relay actually forwards both the sign and the reliability of $x_R$; a large positive $x_R$, for example, means that the XOR value $x_1 \oplus x_2$ has a high probability of being 1. Similar to the water-filling algorithm, the symbol $x_R$ is transmitted with a high power when the reliability is high and with a low power when the reliability is low. From this view of point, MMSE estimate is a power allocation scheme for PNCF. Due to this power allocation, MMSE estimate performs well under a total power constraint. For example, the optimality of MMSE estimate for the one-way relay channel was established in [24].

We end this section by mentioning that compute-and-forward [13,14] with nested lattice code is a form of PNCF in which channel coding has been incorporated. Our discussion of channel-coded PNC in Section 3.2 will focus on PNCF. The information-theoretic discussion in Section 4 will draw on the results of channel-coded PNC using nested lattice code.

### 3.1.2. PNCI

In ANC, $z_R = h_{1R} x_1 + h_{2R} x_2$, what actually gets sent by the relay is $x_R = \hat{z}_R = g \cdot y_R = g \cdot (h_{1R} x_1 + h_{2R} x_2 + u_R)$, where $g$ is the amplification applied by the relay before forwarding the signal. As explained in [10], ANC can be considered as using a linear MMSE estimator. In general, various different estimates in PNCI are also possible (e.g., general MMSE rather than linear MMSE [10]).

Ref. [10] showed that typically PNCF has better performance than PNCI when the uplink is good and the bottleneck is the downlink. Conversely, PNCI has better performance than PNCF when the downlink is good and the bottleneck is the uplink. This is not difficult to understand intuitively. When the uplink is good, the uplink noise

### Table 2

Examples of PNC mappings under each classification.

| Target symbol, $z_R$ | Transmitted output, $x_R = \hat{z}_R$ |
|----------------------|--------------------------------------|
| Analog               | Discrete                             |
| PNCF                 | Estimate (e.g., MMSE) [10,23]         | XOR [1] denoising map [11] |
|                      | Compute-and-forward with lattice code [13,14] |
| PNCI                 | ANC (i.e., linear MMSE) [6,7]         | Other estimates (e.g., MMSE) [10] |
|                      | Compress-and-forward [15]             |                                    |
is relatively small compared with the uplink signals. For example, XOR mapping of \( h_{1R}x_1 + h_{2R}x_2 + w_R \) to \( x_1 \oplus x_2 \) [1] is almost perfect. The small noise is removed by the hard decision of the mapping so that the relay does not expend its transmit power on the uplink noise during the downlink transmission. The BER performance of the whole PNC set-up is reduced to the BER performance of a point-to-point communication system consisting of only the downlink. With PNCI, such as ANC [6], the noise at the relay will be amplified along with the signal. Some transmit power of the relay is used to carry the uplink noise. Thus, the BER performance will be worse than that of the BER performance of a point-to-point link consisting of the downlink alone. Ref. [10] presented results showing that when the uplink and downlink SNR are equal at 5 dB, PNCI has slightly better BER performance than PNCF.

Conversely, when the uplink is bad, the XOR mapping of \( h_{1R}x_1 + h_{2R}x_2 + w_R \) to \( x_1 \oplus x_2 \) is error-prone, while the downlink is not. Self-information at node 1 and node 2 is not of much use when the XOR information transmitted by the relay is erroneous to start with. Meanwhile, the hard decision at the relay removes useful soft information that can be combined with the self-information at the end nodes to improve final decoding. PNCI, such as ANC, passes along the soft information and defers the decision until after the transmission on the downlink is completed. Thus, PNCF tends to perform less well than PNCI when the downlink is good but the uplink is not.

The above discussion on PNCF versus PNCI has focused on non-channel-coded PNC. For channel-code PNC, an advantage of PNCF over PNCI is that PNCF is amenable to link-by-link channel coding using conventional channel codes. Further discussion can be found in Section 3.2.

We end this section by commenting that compress-and-forward [15] is a form of channel-coded PNC. In compress-and-forward, the ANC signal \( g \cdot (h_{1R}x_1 + h_{2R}x_2 + w_R) \) is quantized and then channel-coded. Thus, although \( z_R \) is continuous, \( x_R = \hat{z}_R \) is discrete and drawn from a finite set. Note that the relay does not actually perform any channel decoding to retrieve the source messages \( S_1 \) and \( S_2 \) or \( f(S_1, S_2) \), a network-coded message of the source message; it just adds another layer of channel coding on \( \hat{z}_R = (\hat{z}_R[n])_{n=1,...,N} \) for the downlink transmission. Correspondingly, the end nodes have to perform channel decoding twice, once on the downlink channel code, and another time on the uplink channel code.

### 3.1.3. Asynchrony non-channel-coded PNC

Let us now examine two types of asynchronies: symbol-level asynchrony and phase-level asynchrony. In the following, we will define the notations when they are first used in our presentation. The reader is referred to the Appendix for the collection of notation definitions in one place.

The situation at the relay is depicted in Fig. 7, where the baseband signals from nodes 1 and 2 are shown. The relative phase offset is embedded in the two complex numbers representing the channel gains, \( h_{1R} \) and \( h_{2R} \). For simplicity, we assume time has been normalized and is expressed in unit of symbol duration. That is, one symbol duration is one time unit. Without loss of generality, we assume the signal of node 1 is ahead of the signal of node 2 by \( \Delta \) symbol, \( 0 < \Delta < 1 \). Note that if node 1 is ahead of node 2 by multiple symbols, we can define some null symbols at the head end of the packet of node 2 and at the tail end of the packet of node 1, essentially making the packets larger; our treatment below can be generalized to that situation with minor modifications.

We will assume that relay \( R \) can estimate \( h_{1R} \) and \( h_{2R} \) so that \( h_{1R} \) and \( h_{2R} \) are treated as known at the relay. However, we do not assume \( a \) priori knowledge of \( h_{1R} \) and \( h_{2R} \) at nodes 1 and 2. This means that they cannot perform precoding to remove the relative phase offset between \( h_{1R} \) and \( h_{2R} \).

Besides phase offset, there could be a frequency offset in the RF used by nodes 1 and 2. This frequency offset will translate to a rotating relative phase offset in \( h_{1R} \) and \( h_{2R} \) for successive symbols. If the frequency offset can be estimated, then the rotating relative phase offset can also be tracked. This basically means that different pairs of symbols from nodes 1 and 2 have different relative phase offsets, but these phase offsets can all be estimated and are therefore known. In the following discussion, for simplicity, we will assume a fixed relative phase offset throughout the packet.

In addition, for simple exposition, we assume the use of the rectangular pulse for carrying the digital symbols in the analog domain. Let \( X_i = (x_{i1}, x_{i2}, \ldots, x_{iN}) \) be the packet from node \( i \), \( i = 1, 2 \). At relay \( R \), the received signal in continuous time in baseband is

\[
y_R(t) = \sum_{n=1}^{N} \left( h_{1R}x_1[n]p(t - n) + h_{2R}x_2[n]p(t - \Delta - n) \right) + w_R(t),\]

where \( h_{1R} = \sqrt{P_1} \) and \( h_{2R} = \sqrt{P_2}e^{i\phi} \) (\( \phi \) is the relative phase offset between nodes 1 and 2); \( p(t) \) is the rectangular pulse \( p(t) = 1 \) for \( -1 < t < 0 \) and \( p(t) = 0 \) otherwise); and \( w_R(t) \) is the AWGN noise. Note that we have assumed the normalization of the symbol duration so that it is one, and that the channels experience flat fading.\(^4\) For simplicity, we further assume power control such that \( P_1 = P_2 = P \). Eq. (11) then becomes

\[
y_R(t) = \sqrt{P} \sum_{n=1}^{N} x_1[n]p(t - n) + x_2[n]p(t - \Delta - n)e^{i\phi} + w_R(t).\]

\(^4\) As mentioned in Section 2.5.4, in frequency-selective channel, OFDM could be used so that essentially flat fading is experienced in each subcarrier. In that case, the treatment here can be considered as that for a subcarrier within an OFDM PNC system. The reader is referred to [22,25] for details on OFDM PNC.
In [26,27], suboptimal sampling was assumed: specifically, with respect to Fig. 7, only the overlapped part of $x_1[n]$ and $x_2[n]$ is sampled, and the useful signal in the overlap of $x_1[n + 1]$ and $x_2[n]$ is not used. Furthermore, the joint effects of symbol and phase asynchronies were not considered. Here we consider the use of an optimal maximum-likelihood decoding method based on the belief propagation (BP) algorithm. The method deals with symbol and phase asynchronies jointly.

We focus on the PNCF in which the goal of relay $R$ is to decode $y_2[n] = x_1[n] \oplus x_2[n], n = 1, \ldots, N$. The estimate $\hat{y}_2[n]$ is drawn from the same set as $y_2[n]$. Specifically, relay $R$ wants to minimize the probabilities of decoding error $P(\hat{y}_2[n] \neq y_2[n]) \forall n = 1, \ldots, N$ based on the observation of $y_R(t)$. We perform integration (matched filtering) on the overlapped symbols for a duration of $\Delta$ and a duration of $(1 - \Delta)$ alternately, with a normalization factor $1/(\sqrt{P(\Delta)}$ and $1/(\sqrt{P(1 - \Delta)})$, respectively. Samples $(2n - 1)$ and $2n$ for $1 \leq n \leq N$, and sample $(2N + 1)$ are then given by

$$y_R[2n - 1] = \begin{cases} 1 & \frac{\Delta}{\sqrt{P(\Delta)}} \int_{y_R(t)dt}^{(n-1)+\Delta} X_N[n] + X_{\tilde{N}}[n]e^{i\phi} + \frac{w_R(t)}{1} \sin \frac{\Delta}{\sqrt{P(\Delta)}} \\ \Delta \int_{y_R(t)dt}^{(n-1)+\Delta} X_N[n] + X_{\tilde{N}}[n]e^{i\phi} + \frac{w_R(t)}{1} \sin \frac{\Delta}{\sqrt{P(\Delta)}} \\ \Delta \int_{y_R(t)dt}^{(n-1)+\Delta} X_N[n] + X_{\tilde{N}}[n]e^{i\phi} + \frac{w_R(t)}{1} \sin \frac{\Delta}{\sqrt{P(\Delta)}} \end{cases}$$

$$y_R[2n] = \begin{cases} 1 & \frac{\Delta}{\sqrt{P(\Delta)}} \int_{y_R(t)dt}^{(n-1)+\Delta} X_N[n] + X_{\tilde{N}}[n]e^{i\phi} + \frac{w_R(t)}{1} \sin \frac{\Delta}{\sqrt{P(\Delta)}} \\ \Delta \int_{y_R(t)dt}^{(n-1)+\Delta} X_N[n] + X_{\tilde{N}}[n]e^{i\phi} + \frac{w_R(t)}{1} \sin \frac{\Delta}{\sqrt{P(\Delta)}} \\ \Delta \int_{y_R(t)dt}^{(n-1)+\Delta} X_N[n] + X_{\tilde{N}}[n]e^{i\phi} + \frac{w_R(t)}{1} \sin \frac{\Delta}{\sqrt{P(\Delta)}} \end{cases}$$

where $X_N[0] = 0,$ and $w_R[2n - 1]$ (also $w_R[2N + 1]$) and $w_R[2n]$ are zero-mean complex Gaussian noise with variance $N_0/(2P(\Delta))$ and $N_0/(2P(1 - \Delta))$, respectively, for both the real and imaginary components. Here, $N_0/2$ is the double-sided power spectrum of the AWGN. For QPSK, $x_1[n] \in \{ (1 + j)/\sqrt{2}, (1 - j)/\sqrt{2}, (-1 + j)/\sqrt{2}, (-1 - j)/\sqrt{2} \}$.

Let us write our sampled observations as $Y_R = (y_R[1], \ldots, y_R[2N + 1])$. We want to find the a posteriori probability $P(x_1[n] \oplus x_2[n]|Y_R), n = 1, \ldots, N$, so that the relay $R$ can compute $x_R[n] = \hat{y}_2[n] = \arg \min_{x_1[n] \oplus x_2[n]} P(x_1[n] \oplus x_2[n]|Y_R), n = 1, \ldots, N,$ for the broadcast signal to nodes 1 and 2. Note that $P(x_1[n] \oplus x_2[n]|Y_R)$ can be found from the joint probability $P(x_1[n], x_2[n]|Y_R)$. Thus, we could focus our attention on finding $P(x_1[n], x_2[n]|Y_R)$.

Let us define a “joint symbol” as $(x_1[i], x_2[j]),$ where $i = j$ or $(j + 1)$. There are altogether $2N + 1$ joint symbols and $2N + 1$ sampled observations in $Y_R = (y_R[1], \ldots, y_R[2N + 1])$. The sample $y_R[i + j]$ gives us some information on the joint symbol $(x_1[i], x_2[j])$. Specifically, we have, for $1 \leq n \leq N$,

$$P(x_1[n], x_2[n - 1]|y_R[2n - 1])$$

Due to symbol misalignment, the successive sampled observations are correlated. For a given joint $(x_1[i], x_2[j]),$ what we are interested in is not $P(x_1[i], x_2[j]|y_R[i + j])$ based on a local sample $y_R[i + j]$, but rather the a posteriori probability $P(x_1[i], x_2[j]|Y_R)$ based on the whole collection of samples $Y_R$. That is, samples other than $y_R(i + 1)$ contains useful information on $(x_1[i], x_2[j])$. This is where the belief propagation (BP) algorithm enters the picture [28].

The idea of BP is that $P(x_1[i], x_2[j]|Y_R)$ for all $(i, j)$ pairs can be obtained from a sum–product algorithm [28] based on the individual observations $P(x_1[i], x_2[j]|Y_R[i + j])$. BP is a general inference method for graph models. Interested readers are referred to [28] for a general tutorial on BP. The structure of the sum–product algorithm is given by the Tanner graph associated with the problem.

The Tanner graph for our problem is shown in Fig. 8. In Fig. 8, for brevity, we denote the joint symbol $(x_1[i], x_2[j])$ by $X_{i,j}$. The correlation between two adjacent joint symbols is modeled by the compatibility functions (i.e., check nodes) $\psi_0(X_{n,n-1}, X_n)$ and $\psi_e(X_{n,n}, X_{n+1,n})$.

$$\psi_0(X_{n,n-1}, X_n) = \begin{cases} 1 & \text{if } x_1[n] \text{ in } X_{n,n-1} \\ 0 & \text{otherwise} \end{cases}$$

$$\psi_e(X_{n,n}, X_{n+1,n}) = \begin{cases} 1 & \text{if } x_2[n] \text{ in } X_{n,n} \\ 0 & \text{otherwise} \end{cases}$$

Once the Tanner graph is found, the standard BP procedure can be applied to generate the associated sum–product algorithm. In this paper, we will not go through this standard procedure. The reader is referred to [18,29] for further details.

BP is in general only an approximate algorithm. However, for Tanner graphs with a tree structure, BP yields the exact solution for the marginal probabilities, and it does so in one iteration of the sum–product algorithm [28]. Our Tanner graph in Fig. 8 has a tree structure. Therefore, BP is a very efficient algorithm for resolving symbol misalignment, and it yields the exact solution for $P(x_1[n], x_2[n]|Y_R)$. From $P(x_1[n], x_2[n]|Y_R)$,
BER of ∆ for bad constellation points. The BER is dominated by the
observation for the 16 combinations of x1[n] and x2[n] can be decoded with high confidence (note: not just the XOR of x1[i] and x2[j], but the individual values of x1[i] and x2[j] can be decoded with confidence). The certainties of x1[i] and x2[j] then propagate to the surrounding symbols via the BP algorithm [18, 29]. For example, say a joint symbol adjacent to (x1[i], x2[j]) is (x1[j], x2[j]) and that (x1[j], x2[j]) is a bad constellation point. For this adjacent symbol, since x2[j] is known with high confidence from the good combination (x1[i], x2[j]), the uncertainty left in (x1[j], x2[j]) is only x1[j]. A bad constellation point is bad only when both the constituent symbols are unknown; once one of the constituent symbols is known with certainty, both the constituent symbols of the bad constellation point can be decoded with confidence [18, 29]. In this way, the certainty can propagate a distance along the chain of joint symbols.

We emphasize that certainty propagation depends on the maintenance of the joint probability P(x1[n] ⊕ x2[n]|yb) throughout the BP decoding process. If the joint probability is collapsed into the XOR probability P(x1[n] ⊕ x2[n]|yb) and a BP algorithm is run over this probability instead, the certainty propagation effect will vanish because of the lack of the knowledge of the constituent symbol.

We conclude our discussion of asynchrony in non-channel-coded PNC by remarking that although phase offset can be detrimental to PNC performance, symbol misalignment makes the system more robust against phase asynchrony. Generally, unless one deliberately attempts to align the symbol, most likely there will be some symbol misalignment in the system. Thus, phase offset may not be as bad as it seems. Also, if one has a mechanism to synchronize the symbol arrival times at the relay, it is actually a better strategy to intentionally desynchronize the timing so that ∆ = 1/2. The strategy of intentional symbol misalignment, however, requires further investigation when the signals are band-limited. For example, when pulse shaping is not rectangular, but say raised cosine, each sample yk[i] may contain information from more than a pair of symbols even after matched filtering. The extent to which symbol offset is good in this case has not been carefully studied.

The use of channel coding will ameliorate the phase asynchrony penalty further. This is because with channel coding, the information on each source symbol is generally embedded in a number of channel-coded symbols through the channel coding process. So, if a particular channel-coded joint symbol at the relay has a bad constellation point, there is a chance that another channel-coded joint symbol that also contains information on a common source symbol is a good constellation point. That is, the diversity

![Tanner graph for finding P(x1[i], x2[j]|yb).](image)

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and certainty propagation effects also enter the picture in the channel-coded case. In Section 3.2.2, we will examine some results. We will see that channel coding can actually turn things around in the other direction so that phase penalty becomes a phase reward, even when the symbols are perfectly aligned at the relay.

3.2. Channel-coded PNC

For reliability, forward error control with channel coding can be used protect the information being transmitted. An issue of interest is therefore how channel coding can be integrated into the PNC system. There are two possibilities: end-to-end channel coding and link-by-link channel coding. The discussion in this section focuses on TWRC.

In the following discussion, we will define notations when they are first used. The reader is referred to the Appendix for the overall collection of notations used in TWRC.

For both end-to-end and link-by-link approaches, the two end nodes channel-code their packets before sending them out. Denote the source packets of nodes 1 and 2 by $S_1 = (s_1[m])_{m=1,...,M}$ and $S_2 = (s_2[m])_{m=1,...,M}$, respectively. After channel coding, they transmit $X_1 = C(S_1) = (x_1[n])_{n=1,...,N}$, $X_2 = C(S_2) = (x_2[n])_{n=1,...,N}$, respectively, to the relay. Here, we assume both end nodes use the same channel code $C(\cdot)$ with redundancy factor $N/M$.

End-to-end and link-by-link channel coding approaches differ in how the relay processes the received information. In the end-to-end approach, the relay does not perform channel decoding and re-encoding. For example, the relay may simply try to recover $x_1[n] \oplus x_2[n]$ in a symbol-by-symbol manner and pass the symbols along to the end nodes. In particular, the correlations among different symbols induced by channel coding are not exploited to improve the reliability of the detected $x_1[n] \oplus x_2[n]$. For the symbol-synchronous case, for example, the detection of $x_1[n] \oplus x_2[n]$ is based on solely on $y_2[n]$ and not on $y_2[k]$, $k \neq n$. At an end node, say node 1, the self-information $(x_1[n])_{n=1,...,N}$ is subtracted the received signal, leaving behind $x_2[n]$ plus noise; after that, channel decoding is applied to recover $s_2[n]$.

In the link-by-link approach, the relay makes use of the correlations among successive symbols induced by channel coding to recover the desired network-coded symbols with more accuracy. Potentially, channel coding and network coding functionalities can be integrated together for better performance. There are many subtleties and nuances on how this can be done. Our focus in this section is on the link-by-link approach. We discuss several options on how to integrate channel coding and network coding at the relay.

For a focus, we assume BPSK or QPSK symbols for $x_1[n]$ and $x_2[n]$. The system model is depicted in Fig. 10. Nodes 1 and 2 send $X_1 = C(S_1)$ and $X_2 = C(S_2)$, respectively. We assume $C(\cdot)$ is a linear code so that $X_1 \oplus X_2 = C(S_1) \oplus C(S_2)$. The observed signal at the relay is $Y_R = y_R[n] = h_{1R}x_1[n] + h_{2R}x_2[n] + w_R[n]$. The symbol error rate performance is depicted in Fig. 9. BER of $x_k[n]$ for QPSK modulated PNC: (a) without symbol asynchrony ($\Delta = 0$); (b) with symbol asynchrony ($\Delta \neq 0$).
For the time being, we assume the symbols are aligned. Section 3.2.2 will discuss the symbol-asynchronous case.

3.2.2 synchronous channel-coded PNC

At the relay, a Channel-decoding-Network-Coding operator CNC(·) [30] produces an estimate for \( S_R = (s_R[m])_{m=1,...,M} \) based on \( Y_R = (y_R[n])_{n=1,...,N} \). That is, the estimate is \( \hat{S}_R = \text{CNC}(Y_R)\). We assume the relay uses the same channel code as the two end nodes. After obtaining \( \hat{S}_R \), the relay performs channel coding on \( \hat{S}_R \) to obtain \( X_R = C(\hat{S}_R) \) for broadcast to nodes 1 and 2.

In general, there are different designs for CNC(·) with different performances and implementation complexities. Much of our discussion on link-by-link channel coded PNC focus on CNC(·) because it is the critical component in the system responsible for noise cleaning and PNC mapping.

**PNC mapping for the channel-coded PNC system**

Although the overall PNC mapping at the relay is \( Y_R \rightarrow X_R \), conceptually, the process can be broken into two steps: (i) \( Y_R \rightarrow \hat{S}_R \) with \( \hat{S}_R = \text{CNC}(Y_R) \); and then (ii) \( \hat{S}_R \rightarrow X_R \) with \( X_R = C(\hat{S}_R) \). Step (ii) is similar to conventional channel coding. Step (i) is the new component introduced by PNC.

We remark that for the downlink broadcast of \( X_R \) to the end nodes, the situation at each end node is the same as that of point-to-point communication. Consider the reception at node 1. Suppose that there is no error in the uplink so that \( \hat{S}_R = S_R \). As long as node 1 decodes \( S_R \) correctly, then after the subtraction of self-information \( S_1 \) from \( S_R \), \( S_2 \) is decoded correctly. Conversely, a symbol error in the decoded \( S_R \) will also result in a corresponding symbol error in the decoded \( S_2 \). Thus, the main subtlety in the overall system lies in the operation of CNC(·) in the uplink communication. Therefore, our discussion in this section will focus on CNC(·) in the uplink.

In the next two subsections, we describe a number of different designs for CNC(·) assuming XOR mapping. As already mentioned, and worth emphasizing again, XOR mapping over BPSK or QPSK is only one form of PNCF. The target network coding in the CNC(·) designs discussed here can be replaced with another form of PNCF other than XOR. That said, the insights obtained from the comparison of different XOR designs also apply to non-XOR designs in general.

**XOR-CD**

The second method for CNC(·) is depicted in Fig. 12. We refer to this scheme as CNC\(_{\text{XOR-CD}}(·)\), or simply as XOR - CD. The acronym XOR-CD refers to a two-step process, in which we first apply symbol-by-symbol PNC mapping on the channel-coded symbols to obtain estimates on the XOR.
XOR-CD exploits a nice property when the same linear channel code is used by nodes 1 and 2. In that case, the same channel-decode operation for point-to-point communication can be used here, as implied by the following results:

\[ C(S_R) = C(S_1) \oplus C(S_2) = X_1 \oplus X_2 \]

\[ S_R = C^{-1}(X_1 \oplus X_2). \]  

(16)

That is, the same channel decoder \( C^{-1}(\cdot) \) as in point-to-point communication can be used for input \( P(x_1[n] \oplus x_2[n])y_R[n] \) to obtain \( S_R = (S_R[m])_{m=1, \ldots, M} \).

This scheme was studied in [35]. It was also investigated in [25] in the context of an OFDM-PNC system. Ref. [30] pointed out that this scheme is suboptimal because the information contained in the observable \( y_R[n] \) is embodied in \( P(x_1[n] + x_2[n])y_R[n] \), and some of the useful information for the operation \( CNC(\cdot) \) is lost in the reduction of \( P(x_1[n] + x_2[n])y_R[n] \) to \( P(x_1[n] \oplus x_2[n])y_R[n] \) in the XOR-CD scheme.

Refs. [14,36] considered a scheme with a similar spirit as XOR-CD, using the nested lattice code instead of XOR. As in here, for lattice-coded PNC, PNC Mapping is first applied on the channel-coded signal received using modulus mathematics before a separate channel-decoding operation. It is shown that the scheme can approach the information capacity of TWRC in the high SNR region. Further discussion of the results of the lattice-coded scheme [14,36,37] can also be found in Sections 4.1.1 and 4.1.2 of this paper. Generally, schemes like this work well in the high SNR regime, but not in the low SNR regime.

Joint CNC

A reason why XOR-CD does not work well in the low SNR regime is that the XOR mapping in the first block in Fig. 12 loses useful information. To circumvent this problem, a possibility is to pass the joint probability distribution \( P(x_1[n], x_2[n])y_R[n] \) to the channel decoder. From the received signal \( y_R[n] = x_1[n] + x_2[n] + w_R[n], P(x_1[n], x_2[n])y_R[n] \) can be computed from the original soft information \( P(x_1[n] + x_2[n])y_R[n] \). Note that \( P(x_1[n], x_2[n])y_R[n] \) does not lose information because \( P(x_1[n] + x_2[n])y_R[n] \) can be recomputed back from \( P(x_1[n], x_2[n])y_R[n] \). On the other hand, \( P(x_1[n] \oplus x_2[n])y_R[n] \) in \( CNC_{\text{XOR-CD}}(\cdot) \) loses information because \( P(x_1[n] + x_2[n])y_R[n] \) cannot be recovered from \( P(x_1[n] \oplus x_2[n])y_R[n] \).

In this paper, we refer to the CNC process that makes use of \( P(x_1[n], x_2[n])y_R[n] \), and that performs the CNC process as an integrated process rather than two disjoint channel decoding and network coding processes, as \( CNC_{\text{XOR}}(\cdot) \), or simply as Joint CNC. It can be shown that Joint CNC and the arithmetic-sum CNC in [30] have the same performance. The arithmetic-sum CNC passes \( P(x_1[n] + x_2[n])y_R[n] \) into the channel decoder rather than \( P(x_1[n], x_2[n])y_R[n] \). Both cases make use of the concept of a “virtual encoder” to design the decoding process that performs channel decoding into network-coded information (as opposed to channel decoding into separate source information). The arithmetic-sum CNC computes \( P(s_1[m] + s_2[m]|Y_R) \), \( m = 1, \ldots, M \) through the sum–product algorithm for a Tanner graph corresponding to a “single-source” virtual encoder that sends out \( x_1[n] + x_2[n], n = 1, \ldots, N \). Then \( P(s_1[m] \oplus s_2[m]|Y_R) \) can be obtained from \( P(s_1[m] + s_2[m]|Y_R) \) in a straightforward manner if \( s_1[m] \) and \( s_2[m] \) are binary. As far as we know, the concept of virtual encoder for PNC application was first proposed in [30]. The Joint CNC schemes makes use of the same concept, but a different virtual encoder structure, to compute \( P(s_1[m], s_2[m]|Y_R) \) rather than \( P(s_1[m] + s_2[m]|Y_R) \), noting that \( P(s_1[m] \oplus s_2[m]|Y_R) \) can also be computed in a straightforward manner from \( P(s_1[m], s_2[m]|Y_R) \) (also, \( s_1[m] \) and \( s_2[m] \) do not have to be binary and \( s_1[m] \oplus s_2[m] \) can be interpreted as a general modulo sum).

The reason for dealing with Joint CNC rather than arithmetic-sum CNC is not so much that the former is more efficient than the latter. Rather, Joint CNC is more general. Besides not limiting \( s_1[m] \) and \( s_2[m] \) to binary values, it is also amenable to a general framework in which the assumption of perfect power control, synchronization, and
precoding can be removed. Since Joint CNC can deal with asynchronies in one shot, we defer the presentation of Joint CNC to Section 3.2.2.

3.2.2. Asynchronous channel-coded PNC

Let us now look at the case where there are symbol and phase asynchronies in the channel-coded PNC system.

Asynchronous XOR-CD

First of all, we note that the synchronous XOR-CD discussed in the preceding section can be extended for asynchronous operation as follows. We first use the asynchronous non-channel-coded PNC method discussed in Section 3.1.3 to obtain \( P(x_1[n] \oplus x_1[n]|y_0) \), \( n = 1, \ldots, N \). This takes care of the asynchrony. Then, we feed \( P(x_1[n] \oplus x_1[n]|y_0) \), \( n = 1, \ldots, N \), as the input to second block in XOR-CD (see Fig. 12). This approach is simple and will have good performance in the high SNR regime. However, it is not optimal in general. First, as in synchronous XOR-CD, the mapping in the first block loses information. Second, the correlations among successive symbols induced by symbol offset and the correlations among symbols induced by channel coding are exploited one after another rather than jointly. By this, we mean that the BP algorithm in Section 3.1.3 and the channel decoding are executed one after another. We will present some results of asynchronous XOR-CD later.

Asynchronous joint CNC

In the following, we consider a framework for asynchronous joint CNC. It turns out the framework can also be used to construct a design for asynchronous MUD-XOR as well. This will be discussed later.

This approach of joint CNC is depicted in Fig. 13. Recall also that the asynchronous PNC decoding method in Section 3.1.3 (for non-channel-coded PNC) also takes as input \( P(x_1[n], x_2[n]|y_0) \), \( n = 1, N \), and, \( P(x_3[n]|y_0) \), \( n = 1, N + 1 \), assuming the use of RA code with repeat factor three.
From $y^k_{[1]}$ in (13), we can obtain the joint probability distributions $P(x_1[n], x_2[n - 1]|y^k_{[2n - 1]}), P(x_1[n], x_2[n]|y^k_{[2n]}), n = 1, N$, and $P(x_2[N]|y^k_{[2N + 1]})$, as in (14), assuming the phase offset $\phi$ can be estimated by the relay and is therefore known. The computation of these probabilities is done by the first block of the system diagram in Fig. 13.

In the second block, we feed these joint probability distributions to a decoder that takes care of the handling of asynchrony, network coding, and channel decoding, in an integrated manner. The design of the second block is embodied in the Tanner graph shown in Fig. 14 [18]. The inputs $P(x_1[n], x_2[n - 1]|y^k_{[2n - 1]}), P(x_1[n], x_2[n]|y^k_{[2n]}), n = 1, N$, and $P(x_2[N]|y^k_{[2N + 1]})$ from the first block are fed to the bottom of the Tanner graph. That is, the $Y_R$ nodes of the Tanner graph feed these inputs as observations in the overall belief propagation (sum–product) algorithm.

The bottom three rows of nodes in Fig. 14 are the same as Fig. 8, which was the design used to deal with symbol and phase asynchronies in non-channel-coded PNC. The part above the bottom three rows is related to the decoding of the source joint symbols. Fig. 14 assumes nodes 1 and 2 use the same RA code with repeat factor three.

The structure of the upper Tanner graph in terms of the connectivity between nodes is actually the same as the Tanner graph for point-to-point communication using the same RA code. In the point-to-point case, there is only one transmitter so that each variable node in the Tanner graph is associated with a variable from one source. In the PNC case, we have two transmitters, and each variable node is associated with a pair of variables from the two sources. We could interpret the upper part in Fig. 14 as a “virtual encoder” that takes as input the source information from the two end nodes.

In Fig. 14, the source joint symbols at the top are $s^{n,m} \triangleq (s_1[m], s_2[m]), m = 1, \ldots, M$. The source joint symbols after 3-repeat and interleaving are $\hat{s}^{n,n} \triangleq (\hat{s}_1[n], \hat{s}_2[n]), n = 1, \ldots, N$ where $N = 3M$. The channel-coded joint symbols produced by the virtual encoders are $\chi^{n,n} \triangleq (x_1[n], x_2[n]), n = 1, \ldots, N$. The $\oplus$ in Fig. 14 is a pairwise 2-tuple XOR. For example, $\chi^{n,n} = \chi^{n-1,n-1} \oplus \hat{s}^{n,n} = (x_1[n - 1], x_2[n - 1] + \hat{s}_1[n], x_2[n - 1] + \hat{s}_2[n], \hat{s}_1[n], \hat{s}_2[n])$. In other words, only the symbols from the same end node (nodes 1 or 2) mix with each other in the upper part of the Tanner graph; symbols from nodes 1 and 2 do not inter-mix there. This mixing is how the real encoders at nodes 1 and 2 perform channel coding.

A sum–product message passing algorithm can then be constructed based on the Tanner graph to estimate $P(s_1[m], s_2[m]|Y_R)$ [18]. Such a message passing algorithm gives us an estimate of $P(s_1[m], s_2[m]|Y_R), m = 1, \ldots, M$, from which we can obtain

$$ P(s_1[m] \oplus s_2[m] = a|Y_R) = \sum_{s_1[m]s_2[m]:s_1[m]s_2[m]=a} P(s_1[m], s_2[m]|Y_R). \quad (17) $$

We then set

$$ \hat{s}_R[m] = \text{arg max}_a P(s_1[m] \oplus s_2[m] = a|Y_R). \quad (18) $$

This corresponds to MAP (also ML) decoding of $s_1[m] \oplus s_2[m]$. The relay then performs channel coding on $\hat{s}_R = (\hat{s}_R[m])_{n=1,\ldots,M}$ to obtain $X_R = (x_R[n])_{n=1,\ldots,N}$ for broadcast to nodes 1 and 2.

We remark that strictly speaking, the computation of $P(s_1[m], s_2[m]|Y_R)$ using the sum–product algorithm is only approximate because the Tanner graph has loops. In general, the exact computation of $P(s_1[m], s_2[m]|Y_R)$ is a tough problem. Consequently, the $P(s_1[m] \oplus s_2[m]|Y_R)$ obtained is also approximate. Thus, this method is an approximate ML decoding of $s_1[m] \oplus s_2[m]$.

**Asynchronous MUD-XOR**

The BP framework for Joint CNC can also be used for a version of asynchronous MUD-XOR. To do so, we run the sum–product algorithm exactly as in Joint CNC. However, we compute $\hat{s}_R[m]$ differently. We first find the ML $(s_1[m], s_2[m])$ from

$$ (\hat{s}_1[m], \hat{s}_2[m]) = \text{arg max}_c P(s_1[m] = c, s_2[m] = d|Y_R). \quad (19) $$

From (19), we compute

$$ \hat{s}_R[m] = \hat{s}_1[m] \oplus \hat{s}_2[m]. \quad (20) $$

This $\hat{s}_R[m]$ is not the ML $(s_1[m], s_2[m])$, but rather the $(s_1[m] \oplus s_2[m])$ obtained from the ML $(s_1[m], s_2[m])$. Thus, in general, the symbol error rate will be higher.

**3.2.3. Numerical results**

We now look at some numerical results assuming QPSK modulation. We adopt the regular RA code with a coding rate of 1/3 in our simulations, as in [30]. In the graphs of BER versus SNR per bit to be presented, for each data point we simulated 10,000 packets of 4096 bits. These 4096 bits are divided into in-phase and quadrature parts, each having 2048 bits.

**Joint CNC**

We first examine the results of Joint CNC, our main interest. Thanks to its approximate ML decoding of $s_1[m] \oplus s_2[m]$, Joint CNC has the best BER performance of $s_1[m] \oplus s_2[m]$. Therefore, it is most revealing as far as the fundamental effects of symbol and phase asynchronies are concerned.

In Fig. 15(a), we show the case in which there is no symbol offset. Recall that in non-channel-coded PNC, phase offset induces a penalty (see Fig. 9(a)). For the channel-coded case, instead of a phase penalty, there is a phase reward. With reference to Fig. 15(a), the BER of $\hat{s}_R[m]$ is actually smaller when $\phi \neq 0$. In Fig. 15(b), we show the case in which there is a symbol offset of $\Delta = 0.5$. The performance is better than when $\Delta = 0$. In addition, the phase reward is larger when $\Delta = 0.5$.

In general, for a given BER performance, the power spread due to different phase offsets is less than 1 dB regardless of $\Delta$. Thus, we see that channel coding has the effect of desensitizing the system performance to the effect of phase offset significantly. That is, in addition to phase reward, there is also phase robustness.

The absence of phase penalty in channel-coded PNC can also be explained by the diversity and certainty of
propagation effects, as in the non-channel-coded PNC with symbol offset. With channel coding, the information on each source symbol is embedded in multiple channel-coded symbols. This is analogous to the situation in the symbol-misaligned non-channel-coded PNC where each source symbol pair with two other symbols from the other end node. The difference in the channel-coded case is that even without symbol offset, the channel coding operation itself spreads the information of a source symbol across many channel-coded symbols. Therefore, even without symbol offset, we have the desirable diversity and certainty propagation effects that can combat bad constellation points (see Section 3.1.3).

A last observation is that, as expected, the BER performance with channel coding is much better than without channel coding. For fair comparison between non-channel-coded PNC and channel-coded PNC, in Fig. 15 (for the latter) we shift the curves by \(10 \log_{10} 3 \text{ dB}\) to the right to take into account that each bit is repeated 3 times in our RA channel coding; that is, the energy in Fig. 15 is energy per source bit, or the total energy of three channel-coded bits.

**XOR-CD**

For comparison, let us now look at the performance of asynchronous XOR-CD. Recall that for asynchronous XOR-CD, the PNC XOR processing is first performed on the channel-coded information (using the asynchronous non-channel-coded PNC method discussed in Section 3.1.3) to obtain \(P(x_1[n] \oplus x_2[n]|Y_n)\), \(n = 1, \ldots, N\); after that, channel-decoding is performed on the soft information of \(x_1[n] \oplus x_2[n]\) to obtain an estimate of \(s_1[m] \oplus s_2[m]\) using the traditional channel decoder for point-to-point communication. The two processes are disjoint.

Fig. 16 shows the BER results of asynchronous XOR-CD. In general, we can see that this scheme, although less complex than Joint CNC, has significantly worse performance. In addition, instead of phase reward, there is phase penalty. Its performance is far from what could be achieved fundamentally. The phase penalty is due to its suboptimality.

**MUD-XOR**

We now look at the performance of asynchronous MUD-XOR. Recall that for our particular implementation of asynchronous MUD-XOR, the same decoding framework as asynchronous Joint CNC is used. Both compute \(P(s_1[m] = c, s_2[m] = d|Y_n)\) using the same Tanner graph; however, they use the computed \(P(s_1[m] = c, s_2[m] = d|Y_n)\) differently to obtain different estimates for \(\hat{s}_n[m]\).

Fig. 17 shows the BER results of asynchronous MUD-XOR. Its performance is slightly worse than that of Joint CNC, but still much better than XOR-CD. In addition, similar phase reward and phase robustness as in Joint CNC are present in MUD-XOR.

For code rate of 1/3 (our case here), the Shannon limit for point-to-point AWGN channel is \(-0.55 \text{ dB}\). This belongs to the low SNR regime. It is therefore not surprising that MUD-XOR performs better than XOR-CD and the results are consistent with our earlier comments and information-theoretic analysis in Section 4 that PNC based on MUD will perform well in the low SNR regime. Nevertheless, Joint CNC is still better than MUD-XOR.

Another observation is that the \(-0.55 \text{ dB}\) Shannon limit corresponds to the cut-set bound for the PNC system. While Turbo code and sophisticated LDPC code can be used to approach the \(-0.55 \text{ dB}\) Shannon limit in a point-to-point system, it is still an open issue whether the \(-0.55 \text{ dB} cut-set bound limit can be approached in the PNC system using Turbo code or more sophisticated LDPC code. The RA code assumed in our numerical studies above is still about 3 dB away from the bound.

---

5 The complexity of Joint CNC under QPSK modulation is due to the 16 possible combination values for each of \(x_1[n], x_2[n]\) and \(G_1[n], G_2[n]\) in the branches of the Tanner graph that the sum–product algorithm has to compute over. That is, for each check node \(\oplus\), we have 256 possible input combinations from the two input messages. For XOR-CD, each branch has only 4 combinations in the channel decoding part, thanks to the XOR operation prior to channel decoding. That is, for each check node \(\oplus\), we only have 16 possible input combinations from the two input messages.
Fig. 16. BER of $\hat{s}_R[m]$ in XOR-CD for QPSK modulated channel-coded PNC using RA code with repeat factor three: (a) without symbol asynchrony ($\Delta = 0$); (b) with symbol asynchrony ($\Delta \neq 0$). Note that $E_b$ is energy per source bit here.

Fig. 17. BER of $\hat{s}_R[m]$ in MUD-XOR for QPSK modulated channel-coded PNC using RA code with repeat factor three: (a) without symbol asynchrony ($\Delta = 0$); (b) with symbol asynchrony ($\Delta \neq 0$). Note that $E_b$ is energy per source bit here.

3.3. To probe further

Channel-coded PNC

Refs. [38,39] considered a setup similar to that of Fig. 13, but with no symbol asynchrony. The issue being studied is whether the complexity of the ML decoding as embodied by the strategy in Fig. 13 can be reduced, with the assumption of the use of convolutional codes rather than RA codes, and BPSK modulation. It was shown that a reduced-state trellis can be constructed to reduce the complexity of the decoder with some performance penalty. We remark that because of the merging of multiple states into the XOR states during the decoding process of the reduced-state trellis, it is possible that the “certainty propagation effect” mentioned in our article here will vanish and that there will be a phase penalty associated with the reduced-state trellis approach. This conjecture remains to be further studied.

Ref. [40] also considered a similar setup as in Fig. 13, albeit with symbol synchronization. The use of Low-Density Parity-Check (LDPC) codes is assumed. As in our paper here, the basic idea is ML decoding. The qualitative results are similar to the results presented here.

In ANC, the relay aims to broadcast $h_{1R}X_1[n] + h_{2R}X_2[n]$, $n = 1, \ldots, N$, to the end nodes. In a simple end-to-end channel-coded ANC system, the relay estimates $h_{1R}X_1[n] + h_{2R}X_2[n]$ on a symbol-by-symbol basis. That is, symbols for different $n$ are estimated independently. This simple strategy does not exploit the correlations among different symbols induced by channel coding. How such correlations can be exploited to improve the estimate of $h_{1R}X_1[n] + h_{2R}X_2[n]$ was investigated in [41].

Ref. [42] investigated a system in which the relay explicitly decodes $S_1$ and $S_2$ in the uplink phase, but uses a combination of XOR and superposition coding for the downlink broadcast case. The focus is on how to deal with asymmetric channels to nodes and 2. Supposition coding has better performance than XOR in the broadcast phase when the downlinks are asymmetric.

Synchronization issues

For non-channel-coded PNC, when the symbol offset is more than one symbol, say $L + \Delta$, the relay can do the following to form the network-coded packet. It can separately decode the head end and tail end of the non-overlapping parts, and then jointly decode the overlapping part using the scheme in Fig. 8 with an offset of $L$ symbols from the beginning of the packet from node 1. The network-coded packet of $N$ symbols can then be formed from the XOR of the head end and tail end, and the XOR of the overlapping part. That is, the final network-coded
packet consists of two parts, as follows:

\[
\begin{align*}
(x_1[1] \oplus x_2[N - L + 1], \ldots, x_1[L] \oplus x_2[N]) \\
(x_1[L + 1] \oplus x_2[1], \ldots, x_1[N] \oplus x_2[N - L]).
\end{align*}
\]

Things are more complicated for channel-coded PNC when the symbol offset is \(L + \Delta\). Ref. [43] considered the case when the convolutional channel-code is used, assuming \(\Delta = 0\). In practice, it may be unrealistic to assume that one can align the symbols so that \(\Delta = 0\) when one cannot even ensure the larger time-scale alignment of \(L = 0\). It will be interesting to study if the system in [43] can be modified incorporate nonzero \(\Delta\). As for the RA code (or LDPC code) considered in this article, the Tanner graph will need to be modified. This will be an interesting subject for further study as well.

To our knowledge, [25] is the first paper that explored OFDM PNC. A version of OFDM PNC was implemented in [22]. Here we explain the main essence and motivations. OFDM and PNC is an interesting combination in that symbol-level synchronization or phase synchronization is not required. OFDM PNC is a natural design that does not require the effect to ensure reliable communication. In summary, the OFDM PNC system will be essential to average out BER performance. The use of channel coding on top of OFDM and PNC is an interesting combination in that symbols from the two subcarriers are aligned and phase is not, different random phase term that is different for different subcarrier \(k\) for different subcarrier \(k\). The overall effect is such that there is a randomization of the phase offset across different subcarriers.

Recall that when symbols are aligned (in this case, the subcarrier symbols are aligned) and phase is not different, different phase offsets may lead to different BER performances (see Fig. 9(a)). This means that some subcarriers will have good BER performance while others will have bad BER performance. The use of channel coding on top of the OFDM PNC system will be essential to average out the effect to ensure reliable communication. In summary, OFDM PNC is a natural design that does not require symbol-level synchronization or phase synchronization between nodes 1 and 2.

That said, RF carrier frequency offset is a potential issue in OFDM PNC. If the RF carrier frequencies used by nodes 1 and 2 are not exactly the same, then there will be inter-subcarrier interference in the frequency domain. Specifically, in Eq. (21), we may not be able to ensure that the RHS is a function of subcarrier \(k\) alone. The relay could perform signal processing such that the term due to node 1, \(H_1[k]X_1[k]\), remains intact, but in that case the term due to node 2, \(e^{-j2\pi \theta x_2[k]}H_2[k]X_2[k]\), will contain inter-subcarrier interferences from the signals on the other subcarriers of node 2. Similarly, if we eliminate inter-subcarrier interference for node 2, node 1 will have inter-subcarrier interference. This is a phenomenon that is absent in point-to-point link, in which if the RF offset between the transmitter and the receiver can be perfectly estimated, then inter-subcarrier can be eliminated altogether. For OFDM PNC, even if both the RF offsets of nodes 1 and 2 (with respect to the relay) can be estimated perfectly, only one of the inter-subcarrier interferences can be eliminated entirely. The strategy to deal with the phenomenon is an interesting topic for further research.

**MIMO PNC**

The use of MIMO in PNC systems can have two benefits: improved throughput performance and/or reduced processing complexity. Ref. [44] investigated MIMO PNC with linear detection to reduce processing complexity and to improve performance. The relay extracts the sum and difference of the two end packets, and then constructs the network-coded packet based on the sum and difference. Ref. [45] analyzed the use of optimal ML decoding at a relay with multiple antennas and concluded that the scheme is much better than the amplify-and-forward scheme.

Ref. [46] analyzed the symbol error rate of a system in which the two end nodes are equipped with two antennas and the relay has only one antenna, assuming the use of Alamouti space–time code. It shows that a diversity order of 2 can be achieved. Ref. [47] also studied a MIMO PNC system with space–time codes. The relay and the two end nodes are each equipped with two antennas.

Refs. [48,49] studied linear precoding techniques for MIMO PNC. The authors showed that a proposed precoding scheme based on nested lattice coding (cf. [14]) can closely approach the cut-set capacity upper bound of a MIMO TWRC.

Refs. [50,51] investigated MIMO ANC schemes in which the relay has multiple antennas and the end nodes have single antenna. Ref. [52] considered a cellular system in which a base station communicates with multiple users via a relay. The base station and the relay are equipped with multiple antennas while the end users are equipped with single antenna.

Refs. [53–60] studied systems in which there are multiple relays interconnecting the two end nodes. When there are multiple relays interconnecting the two end nodes, either a relay selection strategy could be adopted, or the multiple relays could work together as a distributed MIMO system.

**Channel estimation**

Channel estimation and RF carrier frequency estimation are important topics in PNC and ANC systems because the detection at the relay and end nodes counts on the knowledge of the channels and RF carrier frequencies used by the end nodes. Note that the RF carrier frequencies of the end nodes may be offset by a small amount which may affect performance if ignored. If known by the relay, the RF carrier offset can be translated into known rotating phase offsets for successful received symbols in the time domain. For OFDM PNC, RF carrier offset is more problematic. Even if known, the carrier offset can cause inter-subcarrier
interference for at least one of the end node’s signal (see discussion under “Synchronization Issues” above). In all cases, unless the RF carrier frequencies used by the transmission and reception at all nodes are synchronized or obtained from the same source, it is important for each receiver to estimate the RF carrier frequencies used by the transmitter.

Refs. [61,62] investigated several channel estimation methods for ANC, in which the relay just amplifies and forwards the composite signal to the end nodes, and channel estimation is done by the end nodes for the round-trip channel. Besides channel estimation, [62] also investigated the estimation of carrier frequency offset between the two end nodes.

Ref. [63] considered a two-phase channel estimation scheme for ANC in which the relay also participates in the channel estimation. The idea is to for the relay to reduce noise (denoise) the uplink channel estimation before forwarding the signal along, so that the channel estimation at the end nodes can be more accurate.

Refs. [64–66] proposed several schemes for channel estimation when OFDM is used. The first two references considered both the estimation of the composite source-relay-source channels (i.e., end-to-end channels from node 1 to node 2 and vice versa) as well as individual channels between sources and relay; the third considered only the composite source-relay-source channels. Blind channel estimation of the composite channels in OFDM PNC was treated in [67].

Ref. [68] analyzed the performance of OFDM ANC systems in which the self-information removal at the end nodes is imperfect. Imperfect self-information removal could be due to imperfect channel estimation, imperfect frame synchronization, and carrier frequency offset.

To tackle the channel estimation challenges in ANC, [69] proposed a blind known interference cancellation scheme. The scheme first cancels the self-interference in a blind way (without the need for complicated channel estimation) using a message passing algorithm. The residual interference is very small after the cancellation process. After the near-perfect cancellation, the target information is then detected as in the conventional point-to-point system.

Multi-way PNC

Beyond TWRC, it is also possible to apply PNC in systems in which more than two end nodes communicate via a relay. Ref. [70] investigated the use of a single relay to interconnect multiple pairs of nodes. To isolate the different pairs, each node pair uses a unique CDMA signature. Then, each node pair uses PNC for information exchange.

Instead of CDMA signatures, [71] made use of multiple antennas at the relay and end nodes to provide the degrees of freedom needed for decoding. The setup studied in [71], referred to as the Y-channel, consists of three end nodes and a single relay. Instead of pairwise communication, each end node has independent information to be transmitted to the other two end nodes.

Refs. [72–75] also considered the setup with multiple end nodes and a single relay. Instead of pairwise communication or each node transmitting independent information to other nodes, a full-exchange broadcast setting is considered. In full-exchange broadcast, each node wants to broadcast the same information to all the other nodes.

By contrast, [76] proposed a general framework, namely, wireless MIMO switching, which can realize arbitrary traffic patterns, not just pairwise or full-exchange. Based on this framework, [77] investigated network-coded relaying schemes for both pairwise and non-pairwise communications.

Other topics

We have not discussed channel-coded SNC thus far. A straightforward way to implement link-by-link channel-coded SNC is to treat the transmissions of the three time slots as being over three independent point-to-point links. In particular, channel decoding into $S_1$ and $S_2$ is performed independently in first two time slots at the relay. Then, $X_R = C(S_1 \oplus S_2)$ is sent in the third time slot. It is also possible to have end-to-end channel-coded SNC. Ref. [78] investigated simple symbol-by-symbol, memoryless processing without explicit channel decoding at the relay. The idea is for the relay to forward soft rather than hard network-coded symbols. Similar ideas for PNC systems are explored in [10,23,79].

Ref. [80] considered the use of OFDM in ANC. It focuses on maximizing the sum capacity by power allocation and permutation of the OFDM tones. Ref. [81] studied the use of OFDM as well as the use of single carrier with frequency domain equalization (SC-FDE) in ANC when channel fading is frequency selective. A result is that SC-FDE has better BER performance than OFDM ANC, but a lower ergonomic capacity.

Refs. [82–84] investigated power allocation and consumption issues in PNC systems.

Refs. [85–89,60] considered the use of noncoherent detection at the relay, in which the channel-state information is not available at the transmitter or receiver. To reduce the penalty due to noncoherent detection, Ref. [60] investigated a system in which multiple relays are installed between two end nodes, and a relay is selected from the multiple relay for amplify-and-forward relaying.

Refs. [90–92] explored the security implication of PNC.

4. Information-theoretic studies

At the most fundamental level, the ultimate network capacity made possible by PNC has to be studied from an information-theoretic perspective. In this article, we restrict our information-theoretic discussions to TWRC. Furthermore, we assume the channels between the two end nodes and the relay are Gaussian channels. For simplicity, we assume the noise powers for all channels are normalized to be one.

4.1. Rate region of Gaussian TWRC

4.1.1. Outer bound for PNC information capacities

Let $C_{1R}$ and $C_{2R}$ be the information capacities of the uplink channels from node 1 and node 2 to relay $R$, respectively. In addition, let $C_{R1}$ and $C_{R2}$ be the information
capacities of the downlink channels from relay $R$ to node 1 and node 2, respectively. In general, we have
\begin{equation}
C_{IR} = \frac{1}{2} \log_2(1 + P_{IR})
\end{equation}
\begin{equation}
C_{RI} = \frac{1}{2} \log_2(1 + P_{RI})
\end{equation}
where $P_{IR}$ is the power received by relay $R$ from node $i$, $i = 1, 2$; and $P_{RI}$ is the power received by node $i$, $i = 1, 2$, from relay $R$.

Let $t_u \geq 0$ be the fraction of airtime dedicated to the uplink phase during which the relay receives from nodes 1 and 2, and $t_d = 1 - t_u$ be the fraction of airtime dedicated to the downlink phase during which the relay transmits to nodes 1 and 2. Let $R_{12}(t_u)$ and $R_{21}(t_u)$ be the information rates from node 1 to node 2 and from node 2 to node 1, respectively, for a given $t_u$. Application of the cut-set bound yields
\begin{equation}
R_{12}(t_u) = \min[t_u C_{1R}, (1 - t_u)C_{R2}] \geq U_{12}(t_u)
\end{equation}
\begin{equation}
R_{21}(t_u) = \min[t_u C_{2R}, (1 - t_u)C_{R1}] \geq U_{21}(t_u)
\end{equation}
where $U_{12}(t_u)$ and $U_{21}(t_u)$ are the upper bounds for $R_{12}(t_u)$ and $R_{21}(t_u)$, respectively. That is, from the information-theoretic viewpoint, given that $t_u$ fraction of the airtime is given to the uplink and $t_d = 1 - t_u$ of the airtime is given to the downlink, the information transfer rate from node 1 to node 2, $R_{12}(t_u)$, cannot exceed $U_{12}(t_u) \geq \min[t_u C_{1R}, (1 - t_u)C_{R2}]$, and the information transfer rate from node 2 to node 1 cannot exceed $U_{21}(t_u) \geq \min[t_u C_{2R}, (1 - t_u)C_{R1}]$. It is unclear at this point whether these upper bounds can be achieved with an appropriate channel code for all SNR. However, we know that these bounds can be approached at the very low SNR regime and high SNR regime. This will be elaborated further when we present the results in Fig. 21 and Table 3.

Fig. 18 shows the trace of a typical locus for the upper bounds ($U_{12}(t_u)$, $U_{21}(t_u)$) as $t_u$ increases from 0 to 1 (the red arrowed lines). In the example, $C_{2R}/C_{R1} \geq C_{R1}/C_{R2}$. When $t_u$ is small, both $U_{12}(t_u)$ and $U_{21}(t_u)$ are limited by the uplink capacities, $t_u C_{1R}$ and $t_u C_{2R}$, respectively. As $t_u$ increases and reaches $t_u = C_{R1}/(C_{2R} + C_{R1})$, then $t_u C_{2R} = (1 - t_u) C_{R1} / C_{R2}$. Beyond $t_u = C_{R1}/(C_{2R} + C_{R1})$, $U_{12}(t_u)$ is still uplink-limited, but $U_{21}(t_u)$ is downlink-limited. As $t_u$ increases further to $t_u = C_{R2}/(C_{R1} + C_{R2})$ and beyond, both $U_{12}(t_u)$ and $U_{21}(t_u)$ become downlink-limited. Thus, for $t_u < C_{R1}/(C_{2R} + C_{R1})$ and $t_u > C_{R2}/(C_{R1} + C_{R2})$, $U_{12}(t_u)$ and $U_{21}(t_u)$ increase and decrease together, and there is no trade-off between them.

Let $C_{2R}$ and $C_{R1}$ be the information capacities from node 1 to node 2, and from node 2 to node 1, respectively. The outer bound for $(C_{12}, C_{21})$ is therefore defined by $(U_{12}(t_u), U_{21}(t_u))$ in the interval $t_u \in [C_{R1}/(C_{2R} + C_{R1}), C_{R2}/(C_{R1} + C_{R2})]$. In Fig. 18, the outer bound is given by the three black lines. The shaded region is the region within which $(C_{12}, C_{21})$ must fall, defined by the following inequalities (besides $C_{12}, C_{21} \geq 0$):
\begin{equation}
\frac{1}{C_{21}} \geq \frac{1}{C_{2R}} + \frac{1}{C_{R1}}
\end{equation}
\begin{equation}
\frac{1}{C_{12}} \geq \frac{1}{C_{R1}} + \frac{1}{C_{R2}}
\end{equation}
\begin{equation}
\frac{C_{21}}{C_{2R}} + \frac{C_{12}}{C_{R2}} \leq 1.
\end{equation}

The interpretation of the first inequality in (24) is as follows. On the RHS, the term $1/C_{2R}$ is the minimum uplink time needed to transmit one bit from node 2 to relay $R$; and the term $1/C_{R1}$ is the minimum downlink time needed to transmit one bit from relay $R$ to node 1. The minimum time for the transport of one bit from node 2 to node 1 must be no less than the sum of these two terms; hence, the inequality. The second inequality in (24) is subject to similar interpretation.

The interpretation of the third inequality in (24) is as follows. This inequality is due to the black line with the negative slope in Fig. 18. On this line, $U_{21}$ is downlink-limited and $U_{12}$ is uplink-limited. Thus, we have $U_{21} = t_u C_{R1}$ and $U_{12} = t_u C_{R2}$. Since $t_u + t_d = 1$, we have $U_{21}/C_{R1} + U_{12}/C_{R2} = 1$. Noting that $C_{21} \leq U_{21}$ and $C_{12} \leq U_{12}$, we have the third inequality in (24).

In the case of $C_{2R}/C_{R1} < C_{R1}/C_{R2}$, the arrows reverse in direction as $t_u$ increases. The negative-sloped black line is one on which $U_{12}$ is downlink-limited and $U_{21}$ is uplink-limited. The first two inequalities in (24) remain the same, but the third inequality is replaced by
\begin{equation}
\frac{C_{21}}{C_{2R}} + \frac{C_{12}}{C_{R2}} \leq 1.
\end{equation}

In the next few sections, we will discuss the extent to which the outer bound of TWRC can be approached by various PNC schemes.

### 4.1.2. Link-by-link channel-coded PNC

We first consider link-by-link channel-coded PNC. We assume the use of nested lattice code. We adopt the results of the nested-lattice-coded scheme in [14] in this discussion. Conceptually, this scheme is similar to the scheme of $C_{NDC}$ in Fig. 12 in that PNC...
mapping is first applied followed by channel decoding in a disjoint manner. For PNC mapping, in place of XOR over superimposed QPSK, we have the modulo operation over nested lattice code in [14]. Rather than calling this scheme \( \text{CNC}_{\text{PNC}, \text{GCD}}(\cdot) \), we shorten it to \( \text{PNC}_{\text{LC}} \) in this section. We will make use of the results from [14] without getting into the details of their derivations. Our goal is to compare the achievable rates with the outer bounds obtained in the preceding section.

With the use of self-information, the achievable downlink rates from relay \( R \) to nodes 1 and 2 are \( R_{\text{PNC,LC}}^{R12} \) and \( R_{\text{PNC,LC}}^{R21} \) respectively, where \( C_{\text{R1}} \), \( C_{\text{R2}} \), \( i = 1, 2 \), are the Shannon information capacities given in (22) [14]. Therefore, the achievable end-to-end information rates by \( \text{PNC}_{\text{LC}} \) are

\[
R_{\text{PNC,LC}}^{R12} (t_u) = \min[t_u R_{\text{PNC,LC}}^{R1}, (1 - t_u) C_{\text{R2}}]
\]

\[
R_{\text{PNC,LC}}^{R21} (t_u) = \min[t_u R_{\text{PNC,LC}}^{R2}, (1 - t_u) C_{\text{R1}}]
\]

(26)

where \( R_{\text{PNC,LC}}^{R1} \) and \( R_{\text{PNC,LC}}^{R2} \) are the uplink capacities when \( \text{PNC}_{\text{LC}} \) is used at the relay \( R \).

Ref. [14] considered the uplink phase and showed that \( R_{\text{PNC,LC}}^{R1} \) and \( R_{\text{PNC,LC}}^{R2} \) can approach the cut-set bounds to within 1/2 bit as depicted in Fig. 19. Specifically, \( R_{\text{PNC,LC}}^{R1} = 1/2 \log_2(1 + \frac{P_{\text{R1}}} {P_{\text{R1}} + P_{\text{R2}} + P_{\text{R1}}}) \) and \( R_{\text{PNC,LC}}^{R2} = 1/2 \log_2(1 + \frac{P_{\text{R2}}} {P_{\text{R1}} + P_{\text{R2}} + P_{\text{R1}}}) \) are achievable; and it can be shown that \( C_{\text{R1}} - R_{\text{PNC,LC}}^{R1} \leq 1/2 \) and \( C_{\text{R2}} - R_{\text{PNC,LC}}^{R2} \leq 1/2 [14].

Fig. 19 also shows, in red dashed lines, the rates achievable by the MUD channel decoding system in which the relay \( R \) explicitly decodes the individual information from nodes 1 and 2. This scheme is similar in spirit to \( \text{CNC}_{\text{MUD}, \text{XOR}}(\cdot) \) in Fig. 11, except that we do not restrict ourselves to QPSK here. We will refer to this strategy as \( \text{PNC}_{\text{MUD}} \) here. In general, \( \text{PNC}_{\text{LC}} \) has good performance in the high SNR region and \( \text{PNC}_{\text{MUD}} \) has good performance in the low SNR region. With convex combination of \( \text{PNC}_{\text{LC}} \) and \( \text{PNC}_{\text{MUD}} \) (i.e., dividing the uplink time among the two strategies), the shaded area in Fig. 19 is the achievable rate region. In particular, the boundary of the shaded area is an inner bound for the achievable rates. For simplicity, for the rest of the discussion in this section, we will not consider such a combination.

Let us now consider the uplink and downlink phases together. Suppose that \( t_u \) is such that both \( U_{12} (t_u) \) and \( U_{21} (t_u) \) in (23), as well as both \( R_{\text{PNC,LC}}^{R12} (t_u) \) and \( R_{\text{PNC,LC}}^{R21} (t_u) \) in (26), are downlink-limited. Then, \( R_{\text{PNC,LC}}^{R12} (t_u) = \min[t_u R_{\text{PNC,LC}}^{R1}, (1 - t_u) C_{\text{R2}}] \) and \( R_{\text{PNC,LC}}^{R21} (t_u) = \min[t_u R_{\text{PNC,LC}}^{R2}, (1 - t_u) C_{\text{R1}}] \). The cut-set bound can be achieved exactly by PNC. Now, suppose that \( t_u \) is such that both \( U_{12} (t_u) \) and \( U_{21} (t_u) \), as well as both \( R_{\text{PNC,LC}}^{R12} (t_u) \) and \( R_{\text{PNC,LC}}^{R21} (t_u) \) are uplink-limited. Then, \( R_{\text{PNC,LC}}^{R12} (t_u) \geq U_{12} (t_u) - t_u / 2 \) and \( R_{\text{PNC,LC}}^{R21} (t_u) \geq U_{21} (t_u) - t_u / 2 \). In general, if \( R_{\text{PNC,LC}}^{R12} (t_u) \) is downlink-limited, then the cut-set bound can be achieved; and if \( R_{\text{PNC,LC}}^{R12} (t_u) \) is uplink-limited, then the cut-set bound can be achieved within \( t_u / 2 \) bit.

Fig. 20 shows the locus of \( R_{\text{PNC,LC}}^{R12} (t_u) \) (blue dashed lines) versus the locus of \( U_{12} (t_u) \) (red dashed lines), reproduced from Fig. 18 as \( t_u \) increases from 0 to 1. For all \( t_u \), \( U_{12} (t_u) - R_{\text{PNC,LC}}^{R12} (t_u) \leq t_u / 2 \).

Achievable symmetric rates in symmetric TWRC

Let us now use the above results to analyze the case in which we target to achieve symmetric rates in both direction; i.e., \( R_{12} = R_{21} \). We assume the simple homogeneous scenario in which all stations use the same transmit power and all channel gains are the same; i.e., \( P_{\text{R1}} = P_{\text{R2}} = P_{\text{R1}} = P_{\text{R2}} = P \).

Let us consider \( \text{PNC}_{\text{LC}} \) first. For the symmetric-rate case, we have \( U_{\text{PNC,LC}} (t_u) = R_{\text{PNC,LC}}^{R12} (t_u) \). Our goal is to find the \( t_u \) that maximizes this transfer rate. To do so, we set the downlink rate to be the same as uplink rate: \((1 - t_u^*) \log_2 (1 + P) = t_u^* \log_2 (1 + P / 2)\), where \( t_u^* \) is the optimal \( t_u^* \). This gives

\[
t_u^* = \frac{ \log_2 (1 + P) } { \log_2 (1 + P) + \log_2 (1 + P / 2) }.
\]

Let

\[
R_{\text{PNC,LC}}^{R12} (t_u^*) = \frac{ R_{\text{PNC,LC}}^{R12} (t_u^*) } { R_{\text{PNC,LC}}^{R12} (t_u) } = \frac{ 1 } { 2 } \frac{ \log_2 (1 + P) } { \log_2 (1 + P) + \log_2 (1 + P / 2) }.
\]

For this symmetric-rate case, the cut-set bound is

\[
U_{12} (1/2) = U_{21} (1/2) = \frac{ 1 } { 4 } \log_2 (1 + P).
\]
Table 3
Achievable symmetric exchange rates for PNC\textsubscript{LC}, PNC\textsubscript{MUD}, SNC, ANC, and TS in symmetric TWRC under equal power usage for all nodes.

| $P$ (dB) | 0  | 2  | 4  | 6  | 8  | 10 |
|----------|----|----|----|----|----|----|
| $R_{12}^{\text{PNC\textsubscript{LC}}}(t_u^*)$ | 0.185 | 0.299 | 0.424 | 0.559 | 0.704 | 0.856 |
| $R_{12}^{\text{PNC\textsubscript{MUD}}}(t_u^*)$ | 0.221 | 0.294 | 0.378 | 0.470 | 0.569 | 0.672 |
| $R_{12}^{\text{SNC}}$ | 0.167 | 0.228 | 0.302 | 0.386 | 0.478 | 0.577 |
| $R_{12}^{\text{ANC}}$ | 0.080 | 0.131 | 0.200 | 0.288 | 0.396 | 0.520 |
| $R_{12}^{\text{TS}}$ | 0.125 | 0.171 | 0.227 | 0.290 | 0.359 | 0.432 |
| $U_{12}(1/2)$ | 0.250 | 0.343 | 0.453 | 0.579 | 0.717 | 0.865 |
| $U_{12}(1/2) - R_{12}^{\text{PNC\textsubscript{LC}}}(t_u^*)$ | 0.065 | 0.044 | 0.029 | 0.020 | 0.013 | 0.008 |
| $U_{12}(1/2) - R_{12}^{\text{SNC}}(t_u^*)$ | 0.029 | 0.049 | 0.075 | 0.109 | 0.149 | 0.193 |
| $U_{12}(1/2) - R_{12}^{\text{ANC}}$ | 0.083 | 0.114 | 0.151 | 0.193 | 0.239 | 0.288 |
| $U_{12}(1/2) - R_{12}^{\text{TS}}$ | 0.170 | 0.212 | 0.253 | 0.291 | 0.321 | 0.345 |
| $U_{12}(1/2) - R_{12}^{\text{MUD}}$ | 0.125 | 0.171 | 0.227 | 0.290 | 0.359 | 0.432 |

Fig. 21. Achievable symmetric exchange rates for PNC\textsubscript{LC}, PNC\textsubscript{MUD}, SNC, ANC, and TS in symmetric TWRC under equal power usage for all nodes.

Fig. 21 and Table 3 summarize the overall results of the achievable rates of various schemes versus $P$. The reader could look at Fig. 21 for the overall trends and Table 3 for more precise numerical values.

Recall that noise power has been normalized to 1, so that $P$ is the SNR. As can be seen, as SNR increases, the gap between the achievable rate by PNC\textsubscript{LC}, $R_{12}^{\text{PNC\textsubscript{LC}}}(t_u^*)$, and the cut-set outer bound $U_{12}(1/2)$ decreases quickly. In general, the larger the SNR, the smaller the gap. It is easy to show from (27) and (28) that $\lim_{P \to \infty} R_{12}^{\text{PNC\textsubscript{LC}}}(t_u^*)/U_{12}(1/2) = 1$. Furthermore, at 10 dB, as indicated by Table 3, the gap is already less than 1%. At low SNR, we see that there is an appreciable gap between $R_{12}^{\text{PNC\textsubscript{LC}}}(t_u^*)$ and $U_{12}(1/2)$, indicating that $R_{12}^{\text{PNC\textsubscript{LC}}}(t_u^*)$ may not be the optimal scheme for PNC when SNR is low. Recall, however, that $R_{12}^{\text{PNC\textsubscript{LC}}}(t_u^*)$ is really a lower bound [14] rather than the achievable rate by nested lattice code. Thus, the actual gap is actually unknown based on the research results to-date.

For comparison, we also include the results for PNC\textsubscript{MUD}. We assume that the downlink capacity ($\log_2(1 + P)$)/2 can be achieved. For uplink, the rate $R_{12}^{\text{PNC\textsubscript{MUD}}} = R_{21}^{\text{PNC\textsubscript{MUD}}} = (\log_2(1 + 2P))/4$.

Thus, the optimal $t_u$ and the achievable rate for PNC\textsubscript{MUD} are

$$t_u' = \frac{\log_2(1 + P)}{\log_2(1 + P) + 0.5 \log_2(1 + 2P)}$$

$$R_{12}^{\text{PNC\textsubscript{MUD}}}(t_u') = R_{21}^{\text{PNC\textsubscript{MUD}}}(t_u') = \frac{1}{4} \cdot \log_2(1 + P) \cdot \log_2(1 + 2P).$$

From Fig. 21 and Table 3, we see PNC\textsubscript{MUD} may have better exchange rate than PNC\textsubscript{LC} at low SNR. At higher SNR, PNC\textsubscript{LC} is better. At 0 dB, the gap relative to the upper bound is 26% for PNC\textsubscript{LC}, and 12% for PNC\textsubscript{MUD}. By contrast, at 10 dB, the gap is less than 1% for PNC\textsubscript{LC}, and 22% for PNC\textsubscript{MUD}. It can be easily shown from (28) and (29) that at extremely low SNR, $\lim_{P \to 0} R_{12}^{\text{PNC\textsubscript{MUD}}}(t_u')/U_{12}(1/2) = 1$. At extremely high SNR, $\lim_{P \to \infty} R_{12}^{\text{PNC\textsubscript{MUD}}}(t_u')/U_{12}(1/2) = 2/3$. That is, the gap goes from 0% at very low SNR to 33% at very high SNR.

We could perform a similar analysis for SNC depicted in Fig. 2. Three time slots are need with each transmission taking the same amount of time. Each of the transmission can achieve the information capacity since each is a point-to-point link. Thus,

$R_{12}^{\text{SNC}} = R_{21}^{\text{SNC}} = \frac{1}{6} \log_2(1 + P).$ 

As shown in Fig. 21 and Table 3, the performance of SNC is not as good as that of PNC\textsubscript{MUD} or PNC\textsubscript{LC} in general. From (28) and (30), we see that $R_{12}^{\text{SNC}}(t_u')/U_{12}(1/2) = 2/3$. Thus, the performance gap is 33% across all SNR.

Let us also take a look at the TS scheme in Fig. 1. Again, we assume link-by-link channel coding. By symmetry, each of the four transmissions uses a quarter of the airtime. The achievable rate is

$$R_{12}^{\text{TS}} = \frac{1}{8} \log_2(1 + P).$$

From (28) and (31), $R_{12}^{\text{TS}}(t_u')/U_{12}(1/2) = 2/3$. Thus, the performance gap is 33% across all SNR.
Let us now reflect on these information-theoretic results. In our earlier discussion in Section 2, based on slot counting, we mentioned that PNC can achieve 100% throughput improvement compared with TS. SNC, on the other hand, can achieve 33% throughput improvement. Strictly speaking, that is true only when the channels are highly reliable so that we do not have to worry about noise. That is, when the SNR is high. Our information-theoretic results here confirm that intuition. When SNR is high, PNC\textsubscript{LC} approaches the upper bound, which has twice the rate of TS. Similarly, when SNR is high, the information-theoretic rate of SNC is 33% that of TS.

At the low SNR regime, PNC\textsubscript{MUD} can also approach the upper bound. Thus, at low SNR, the information rate of PNC is still twice that of TS. This is in contrast to the use of ARQ for error control, in which the throughput of PNC is only 33% above that of TS at the very low SNR end (see Section 2.5.1).

As indicated in Table 3, there is still an appreciable gap for PNC in the mid SNR range. This appears to be a fertile ground for future research. Recall that PNC\textsubscript{MUD} and PNC\textsubscript{LC} are similar to MUD-XOR and XOR-CD in Figs. 11 and 12, respectively, in that the network coding and channel decoding operations are disjoint. They tend to work well only in the low and high SNR regimes, respectively. The design in Fig. 13, on the other hand could work well under all SNR regimes; however, they are only limited to XOR over QPSK.

A gap that remains to be filled in the information-theoretic study is whether an upper-bound approaching scheme is available for all SNR regimes. For example, is there a lattice-code design similar to that of Fig. 13 that can work well under all SNR regimes? What is the ultimate fundamental capacity region for PNC-based TWRC?

4.1.3. End-to-end channel-coded ANC

We now look the amplify-and-forward ANC scheme [6] in which the relay is not involved in channel decoding and re-encoding. Channel coding is applied on an end-to-end basis.

Recall that in the ANC scheme in [6], the relay just amplifies and forwards the received signal. It is reasonable to assume that a chunk of frequency band has been allocated to the system as a whole. In a time division system, the uplink and downlink take turns to use the bandwidth, and they have the same available bandwidth. In the simple ANC system in [6], each uplink symbol is amplified and mapped to a downlink symbol so that the uplink and downlink symbols have the same format (e.g., if uplink uses QPSK, so does downlink). In this case, the available bandwidth dictates the symbol duration. Thus, the symbol durations in the uplink and downlink are the same. This means that \( t_1 = t_2 = 1/2 \).

Not being able to adjust the durations of \( t_1 \) and \( t_2 \) is one shortcoming of ANC because one loses a degree of freedom in the system design [20]. A second shortcoming is that with only end-to-end channel coding, the relay cannot remove codeword errors incurred by the uplinks before forwarding the data.

Let us derive the information rate for the end-to-end channel-coded ANC. At the relay, the signal powers received from nodes 1 and 2 are \( P_{1R} \) and \( P_{2R} \), respectively. Recall that we normalize noise power to be one unit. Let \( P_k' \) be the transmission power of the relay. We have

\[
P_k' = \alpha \cdot (P_{1R} + P_{2R} + 1)
\]

for some amplification factor \( \alpha \). At node 1, the received power is \( P_{R1} = P_k' |h_{R1}|^2 \) where \( h_{R1} \) is the channel gain for the channel from relay \( R \) to node 1. Similarly, the received power at node 2 is \( P_{R2} = P_k' |h_{R2}|^2 \). We assume the receiver noise powers at node 1 and node 2 are also one unit.

At node 1, after subtracting the self-information, the signal power is \( \alpha |h_{R1}|^2 \). The noise power, including the accumulated at the relay and the noise at node 1, is \( \alpha |h_{R1}|^2 + 1 \). Hence, the SNR at node 1 (and similarly, SNR at node 2) is

\[
SNR_1 = \frac{\alpha P_{2R} |h_{R1}|^2}{\alpha |h_{R1}|^2 + 1} = \frac{P_{2R} P_{R1}}{P_{R1} P_k' |P_k'| + 1} = \frac{P_{2R} P_{R1}}{P_{R1} P_k' R_{1} R_{21}}
\]

\[
SNR_2 = \frac{P_{R2} + P_{2R} + P_{1R} + 1}{P_{R2} + P_{2R} + P_{1R} + 1}
\]

Since each of the uplink phase and downlink phase uses up half the airtime, we have

\[
R_{21}^\text{ANC} = \frac{1}{4} \log_2 \left( 1 + \frac{P_{2R} P_{R1}}{P_{R1} P_k' R_{1} R_{21}} \right)
\]

\[
R_{12}^\text{ANC} = \frac{1}{4} \log_2 \left( 1 + \frac{P_{1R} P_k' R_{2} R_{12}}{P_{R2} + P_{2R} + P_{1R} + 1} \right)
\]

Let us now look at symmetric TWRC in which \( P_{1R} = P_{2R} = P_{R1} = P_{R2} = P \). Then,

\[
R_{21}^\text{ANC} = R_{12}^\text{ANC} = \frac{1}{4} \log_2 \left( 1 + \frac{P^2}{3P + 1} \right)
\]

The results for ANC are also shown in Fig. 21 and Table 3. We see that from an information-theoretic standpoint, end-to-end channel-coded ANC does not work as well as other link-by-link channel-coded PNC scheme. The performance gap relative to the upper bound ranges from 68% for 0 dB to 40% for 10 dB. It can be easily shown, however, that at extremely high SNR (as \( P \to \infty \)), the performance gap for ANC reaches a constant of 0.396 bits. Thus, percentage-wise, the performance gap goes to zero at extremely high SNR region. At low SNR, ANC does not perform well. This is understandable. At low SNR, the noise at the relay is high relative to the signal. Much of the downlink power is used to carry this noise to the two end nodes.

4.2. Energy implications for Gaussian TWRC

PNC was originally conceived as a capacity boosting mechanism. In TWRC, SNC requires three transmissions for the exchange of a packet (one in each direction) between nodes 1 and 2. Traditional TS requires four transmissions. Thus, the energy saving for SNC is 25%. Although PNC saves an additional time slot, three transmissions are also needed (once each by nodes 1, 2, and R). Thus, it may appear at first
glance that there is no additional energy saving beyond that SNC. That turns out to be not the case.

In this section, we look at the issue more fundamentally from an information-theoretic perspective. The key idea is to convert capacity increase in PNC to energy saving. We argue that for the same exchange rate, PNC can achieve significant transmit energy saving in the high SNR regime. Our discussion here only considers the transmit energy. In a real system, there will be receiver energy and processing energy to consider as well. In that light, the discussion in this paper is only a preliminary foray into a new research direction.

Let us look at the symmetric TWRC again, in which the channel gains are all equal: \( h_{1R} = h_{2R} = h_{R1} = h_{R2} \). Our analytical approach is that we keep the rates of all schemes equal, and then compare their energy usage. For simplicity, we assume the energies used by all nodes are equal. Specifically, in our analysis we allow the transmit powers to be different for the uplink and downlink phases, but adjust the uplink time \( t_{u} \) and downlink time \( t_{d} \) such that node 1, node 2, and relay \( R \) use the same energy. We target to have symmetric rates (i.e., equal rate in both directions).

Consider SNC. We assume that each of the three transmissions can achieve rate equal to Shannon capacity. Thus, \( 1/3 \) of the airtime is dedicated to each phase. Thus, the energy expended by each node is \( E_{SNC} = P_{SNC}/3 \), where \( P_{SNC} \) is the power of each node. For a given exchange rate target \( R \), we have that

\[
R = R_{12}^{SNC} = R_{21}^{SNC} = \frac{1}{6} \log_{2}(1 + P_{SNC})
\]

\[= \frac{1}{6} \log_{2}(1 + 3E_{SNC}). \tag{36} \]

For PNC, we will consider both PNC\(_{LC} \) and PNC\(_{MUD} \) discussed in the preceding section. For PNC\(_{LC} \) and PNC\(_{MUD} \), in order that nodes 1 and 2 use the same energy as relay \( R \), we allow \( P_{1R}^{PNC_{LC}} = P_{2R}^{PNC_{LC}} \neq P_{R1}^{PNC_{LC}} = P_{R2}^{PNC_{LC}} \)

\( P_{1R}^{PNC_{MUD}} = P_{2R}^{PNC_{MUD}} \neq P_{R1}^{PNC_{MUD}} = P_{R2}^{PNC_{MUD}}. \)

We first explain the numerical method we use for PNC\(_{LC} \). For a given rate requirement \( R \), we have

\[
R = t_{u} \cdot \frac{1}{2} \log_{2} \left( 1 + P_{1R}^{PNC_{LC}} \right)
\]

\[= (1 - t_{u}) \cdot \frac{1}{2} \log_{2} \left( 1 + P_{R1}^{PNC_{LC}} \right). \tag{37} \]

The energies used by node 1 (or node 2) and the relay are

\[E_{1}^{PNC_{LC}} = t_{u} P_{1R}^{PNC_{LC}} \]

\[E_{R}^{PNC_{LC}} = (1 - t_{u}) P_{R1}^{PNC_{LC}}. \tag{38} \]

For numerical computation, for a given \( R \) in (37), we vary \( t_{u} \) from 0 to 1. For each \( t_{u} \), we compute \( P_{1R}^{PNC_{LC}} \) and \( P_{R1}^{PNC_{LC}} \) according to (37). Then, we check if the two energies in (38) are equal based on the \( P_{1R}^{PNC_{LC}} \) and \( P_{R1}^{PNC_{LC}} \). We identify the \( t_{u} \) at which the equality \( E_{1}^{PNC_{LC}} = E_{R}^{PNC_{LC}} \) is achieved, and this is the solution for a given \( R \).

For PNC\(_{MUD} \), corresponding to (37), we have

\[
R = t_{u} \log_{2}(1 + 2P_{1R}^{PNC_{MUD}}) = \log_{2}(1 + P_{R1}^{PNC_{MUD}}).
\]

Corresponding to (38), we have

\[E_{1}^{PNC_{MUD}} = t_{u} P_{1R}^{PNC_{MUD}} = (1 - t_{u}) P_{R1}^{PNC_{MUD}} \triangleq E_{R}^{PNC_{MUD}}. \tag{39} \]

This gives the following closed-form without the need for numerical computation:

\[
R = \frac{1}{6} \log_{2}(1 + 3E_{PNC_{MUD}}). \tag{40} \]

Note that (40) is similar to (36). Thus, PNC\(_{MUD} \) has the same energy performance as SNC.

For end-to-end channel-coded ANC, the power used by all three nodes should be equal in order that they use the same energy. For a target rate \( R \), we have \( R = \frac{1}{6} \log_{2}(1 + \frac{2P_{ANC}^{2}}{3P_{ANC} + 1}) \). In addition, \( E_{ANC} = \frac{1}{6} P_{ANC} \). This gives

\[
R = \frac{1}{6} \log_{2} \left( 1 + \frac{(2E_{ANC}^{2})^{2}}{6E_{ANC} + 1} \right) \tag{40} \]

where \( P_{ANC} \) and \( E_{ANC} \) are the power and energy used by each node.

Finally, we consider TS in Fig. 1. Half of the uplink time is given to the transmission of node 1, and half the downlink time is given to the transmission of relay \( R \) to node 1. Thus, the rate is \( R = \frac{1}{2} \cdot \frac{1}{2} \log_{2}(1 + P_{TS}) = R = \log_{2}(1 + 2P_{1R}^{TS}) \). Equating the energy usages of all the nodes, we have

\[E_{1}^{TS} = \frac{1}{2} P_{TS} = (1 - t_{u}) P_{R1}^{TS} = E_{R}^{TS} \triangleq E_{TS} \tag{37} \]

(note that the relay transmits twice in the downlink phase, once to each end node). We use a numerical method similar to the one used for PNC\(_{LC} \) above to find the solution.

In Table 4, we use SNC as the benchmark starting point. We vary \( P_{SNC} \) from 0 dB to 10 dB and compute the resulting \( R_{SNC} \) according to (36). We fix the target rate \( R = R_{SNC} \) and then use the above methods to compute the energy requirements for PNC\(_{LC} \), PNC\(_{MUD} \), and ANC.

From Table 4, we see that in the high SNR regime (i.e., the high rate regime), PNC\(_{LC} \) is most energy efficient. However, at the lower SNR (low rate) regime, PNC\(_{MUD} \) and SNC have the most efficient energy usage. ANC is not energy efficient for the SNR range investigated here. In

| Table 4 | Energies needed for PNC\(_{LC} \), PNC\(_{MUD} \), SNC, ANC, and TS in symmetric TWRC under equal energy usage for all nodes. |
|---------|---------------------------------|
| \( P_{SNC} \) (dB) | 0 | 0.1667 | 0.2284 | 0.3020 | 0.3861 | 0.4783 | 0.5766 |
| \( E_{SNC} \), \( E_{PNC_{MUD}} \) (dB) | -4.771 | -2.771 | -0.771 | 1.229 | 3.229 | 5.229 |
| \( E_{PNC_{LC}} \) (dB) | -1.522 | -1.024 | -0.342 | 0.648 | 1.900 | 3.264 |
| \( E_{SNC} \) (dB) | 0.105 | 1.688 | 3.264 | 4.819 | 6.345 | 7.840 |
| \( E_{TS} \) (dB) | -1.928 | 0.160 | 2.341 | 4.618 | 6.987 | 9.432 |
particular, it can be even less efficient than TS in the low SNR regime.

4.3. To probe further

The ANC rates in (35) are derived assuming the relay estimates \( h_{18}x_1[n] + h_{28}x_2[n] \) for different \( n \) independently. With this memoryless estimation assumption, detailed information-theoretic analysis demonstrating the advantage of ANC over the traditional relaying techniques can be found in [93]. The rates for a non-memoryless ANC relay which exploits correlation among symbols induced by channel coding [41] would be better than the rates in (35). The exact information rates for non-memoryless ANC, however, remain an open issue.

Ref. [50] investigated the capacity region of a MIMO ANC system in which the two end nodes have one antenna, and the relay has multiple antennas. Linear processing is assumed at the relay. The correlations among symbols within a packet due to channel coding are not exploited to boost performance.

There is a body of works related to a technique called compress-and-forward (CF) [15,94–96]. In CF, the relay first compresses the received packet \( Y_R \) to \( Y_R' \), and then encodes \( Y_R' \) into a packet \( X_R \) for broadcast to nodes 1 and 2. An end node first decodes \( Y_R' \) from the received signal, and then decode the packet from the other end node based on \( Y_R' \). The intuition of CF is that the relay tries to decrease (clean up) the uplink noise by some hard decision. The quantized information can be channel-coded before forwarding. Channel coding at the relay helps to achieve the downlink channel capacity (part of which is given to the remaining noise and part of which is given to the information). Since the hard decision can be adapted to the uplink noise, it may work well at different SNR for the uplink. However, it is suboptimal in the downlink. The reader is referred to [15], in which the achievable rate regions for TWRC under various relaying techniques, including ANC, explicit-decode-and-forward, and CF, were derived and compared.

Ref. [95] showed that rates within \( \log_2 3 \) bit of the outer bound can be achieved by a combination of amplified-and-forward, CF, and superposition coding. By contrast, [14] showed that rates within \( 1/2 \) of the cut-set outer bound can be achieved under AWGN channels by incorporating network-coding mapping with lattice code.

To our best knowledge, the ultimate capacity region for PNC-based systems is still an open issue. The design in [14] is a design similar in spirit to the XOR-CD scheme in that the network coding operation and the channel decoding operation in the relay are disjoint. The network coding operation performed prior to channel decoding loses much useful information, and the scheme only approaches the outer bound in the high SNR regime.

Refs. [58,97–99] studied the case where the relay obtains explicit information on \( S_1 \) and \( S_2 \); and in the downlink broadcast phase, the relay needs to encode \( (S_1, S_2) \) into \( X_R \) so that nodes 1 and 2 can decode \( S_2 \) and \( S_1 \), respectively with side information. The explicit decoding of \( S_1 \) and \( S_2 \) at the relay in the uplink phase corresponds to the MUD scheme, which is embodied in the design of...
5.1. Asymptotic performance analysis

In this section, we discuss the feasibility and throughput superiority of PNC in 1-D and 2-D wireless networks with $N$ nodes. In our analysis, half of the nodes are randomly selected as the source nodes and the remaining other half are the sink nodes. We assume we want to deliver equal amounts of traffic for all the $N/2$ flows. We derive the asymptotic throughput per flow for large $N$.

We adopt the well accepted physical interference model in [105]. Specifically, we assume that the transmission of a link is successful if and only if the SIR is more than a given threshold, say 10 dB. In addition, we impose the half-duplex constraint in our system model (i.e., a node cannot transmit and receive at the same time).

We first investigate the 1-D regular topology in which the nodes are regularly spaced. We show that the throughput of PNC can approach the theoretical upper bound asymptotically as $N$ goes to infinity. We then extend the analysis to the 1-D random topology in which nodes are not regularly spaced. We show that the asymptotic results remain valid for the 1-D random topology if a hierarchical routing scheme is adopted. We further extend our analysis to the 2-D regular and random topologies.

Before we delve into the details, let us give the broad picture. Recall that in Section 2.5.6, we briefly overviewed the use of virtual paths as a decomposition method for constructing bidirectional and unidirectional PNC flows in a general network topology. Each virtual path may contain many flows, and a virtual path is like a 1-D network since it traverses a sequence of nodes. Thus, after the decomposition, the overall network consists of many 1-D networks conceptually. This is also the main idea in the progression of our presentation below. In particular, we start with the 1-D networks and then apply the results to 2-D networks. There are many ways to construct virtual paths. The method we outline below is a simple but not necessarily the optimal method.

**Topology 1: regular 1-D network**

Consider a regular 1-D linear network topology in which the $N$ nodes are regularly spaced such that the distance between any two adjacent nodes is a constant, as shown in Fig. 22. There are altogether $N/2$ flows in the network with half the nodes randomly chosen as the sources and half the nodes randomly chosen as the destinations. Two issues are of interest: (1) how to apply PNC to the $N/2$ flows; and (2) what is the asymptotic throughput per flow for such a PNC system as $N \to \infty$.

For our $N/2$ flows in the 1-D network, the basic idea is as follows. First, we note that some flows are in one direction and some flows are in the opposite direction. If we observe $\alpha$ units of traffic (possibly from different flows) along a sequence of links, say links $i, i + 1, \ldots, j - 1, j$; and also $\alpha$ units of traffic along the sequence of links $j, j - 1, \ldots, i + 1, i$ in the opposite direction, then we could aggregate the traffic in the two opposing directions for transport over a bidirectional PNC virtual path. We can then apply PNC scheduling as in Fig. 5 to this PNC bidirectional virtual path to reduce the number of time slots needed. An issue, of course, is the optimal way to form PNC virtual paths out of the $N/2$ flows. In what follows, instead of seeking an optimal algorithm, we simply use a heuristic algorithm for our asymptotic study. And this heuristic can achieve the optimal throughput per flow asymptotically.

In our heuristic, instead of aggregating many flows into each PNC virtual path in one shot, we incrementally aggregate traffic of only two flows in opposing directions. That is, we will construct mini bidirectional virtual paths, each containing only traffic of only two flows in opposing directions. These mini bidirectional virtual paths could later be aggregated into larger virtual paths for operation purposes. We refer to the mini bidirectional virtual path as a "PNC unit". An overall PNC bidirectional virtual path consists of a bundle of mini bidirectional virtual paths on the same sequence of nodes. An example of a PNC unit could simply be the three-node TWRC we have discussed in the previous sections. More generally, a PNC unit is a linear chain of multiple nodes, for which the PNC mechanism can be applied.

To form PNC units, we introduce the concept of "packings". The reader is referred to Fig. 22 for illustration. A right packing consists a sequence of non-overlapping right-bound flows from left to right in the 1-D network. Similarly, a left packing consists a sequence of non-overlapping left-bound flows from right to left. In Fig. 22, Flow 1 belongs to a right packing, and Flows 2 and 3 belong to a left packing. In general, we can form many "tight" right packings in a greedy way. We start from the left of the 1-D network and look to the right. Upon encountering the source node of the first right-bound flow, we include the flow into a right packing. Then, we continue to look to the right beyond the destination of the first right-bound flow to find the next right-bound flow. We repeat this until we reach the right end of the 1-D network. We then have a right packing consisting of a sequence of non-overlapping right-bound flows. To form the next right packing, we repeat the above procedure for the remaining right-bound flows. We do this until we have a set of right packings. Left packings are constructed similarly by progressing from right to left.

A dual packing is formed by matching a right packing and a left packing. Suppose that we have $R$ right packings and $L$ left packings. Then the number of dual packings is $M = \min(R, L)$. The numbers of unmatched right and left packings are respectively $R - M$ and $L - M$, one of which must be zero; equivalently, the number of unmatched unidirectional flows is $R + L - 2M$.

Fig. 22 shows an example of a dual packing. Flows 2 and 3 are part of a right packing in the 1-D network, and Flow 1 is part of a left packing. Note that some of the nodes are traversed by both a right-bound flow and a left-bound flow. We call these nodes the common nodes, and the other nodes the non-common nodes. A sequence of adjacent
common nodes in between two non-common nodes (an ellipse in Fig. 22) forms a PNC unit. A sequence of adjacent non-common nodes in between two common nodes at the boundary (a rectangle in Fig. 22) may or may not have traffic flowing over them. When there is traffic, the traffic is in one direction only, and the traditional multihop store-and-forward scheme or the unidirectional PNC scheme [1] can be used to carry the unidirectional traffic.

The set of dual packings yield a set of mini virtual bidirectional flows (each corresponding to a PNC unit) and some residual unidirectional virtual flows. Thus, our construction results in two types of entities: (1) PNC units that can exploit the bidirectional PNC mechanism; (2) unidirectional flows consisting of the above residual unidirectional virtual flows and the aforementioned R + L − 2M unmatched unidirectional flows. Our scheduling strategy is described below.

Recall that we want to deliver equal amounts of traffic for all the N/2 flows. Our scheduling is frame-based. Each frame consists of F time slots. Within the F time slots, each of the N/2 flows will deliver one packet from its source to its destination. The throughput per flow is therefore 1/F.

A frame is divided into two intervals as follows:

1. The first interval is dedicated to the PNC units. Note that with M dual packings, 2M time slots are needed in the worst case. To see this, we note that in the worst case, the PNC units in different dual packings use different time slots to transmit. The PNC units in the same dual packing can be scheduled to use the same two time slots because they are non-overlapping in space; for each PNC unit, by pipelining (as in Fig. 5), within two time slots a packet will reach each end node.\(^6\)

2. The second interval is dedicated to the aforementioned unidirectional flows. They will make use of the traditional multihop scheme for data transport.

As argued in [103], the frame length is dominated by the first interval above asymptotically as N goes to infinity.

**Theorem 1.** With PNC, we can approach the upper bound of the per-flow throughput of the 1-D regular network. Specifically, the throughput per flow is the following with high probability.

\[
\lambda_{\text{PNC}} = 4/N - \varepsilon = 4/N - O(1/\log(N))/N. \tag{41}
\]

That 4/N is an upper bound in the half-duplex 1-D network can be seen from the fact it corresponds to a situation in which the bottleneck link is busy all the time.\(^7\) For a detailed proof on how PNC can approach this upper bound, see [103].

It can be shown that the throughputs per flow for TS and SNC for large N are 2/N and 8/(3N) [103]. Thus, PNC can improve the asymptotic throughput of the 1-D network by a factor of 2 and 1.5 relative to the traditional transmission scheme and the SNC scheme, respectively [103]. Note that this is the same improvements as observed in TWRC with only two flows.

For simplicity, we have assumed that the source and destination nodes of the N/2 flows are distinct. Theorem 1 can be extended to the case in which the source and destination of each flows are randomly selected among the N nodes with equal probability. In other words, a node may be the source or destination of multiple flows, or it may be not an end node at all. Theorem 1 below is the corresponding modified version of Theorem 1. The asymptotic result remains the same.

**Theorem 1’.** With PNC, we can also approach the upper bound of the per-flow throughput of the 1-D regular network when the source and destination nodes are randomly selected from the N nodes with equal probability. Specifically, the throughput per flow is the following with high probability.

\[
\lambda_{\text{PNC}} = \frac{4}{N} - \varepsilon = \frac{4}{N} - \frac{O(1/\log(N))}{N}. \tag{42}
\]

The proof of this theorem is similar to that of Theorem 1 and it is omitted here.

**Topology 2: random 1-D network**

We now extend the schemes in the regular 1-D network to the random 1-D network where the N nodes are randomly distributed over the line. Specifically, each node is randomly placed on the 1-D line with uniform distribution, and the placements of the nodes are independent.

We propose a transmission scheme inspired by [106] and [107]. In this scheme, we form a hierarchical network in which some nodes are selected to be routing nodes. In selecting the routing nodes, we ensure that they are almost evenly located to form a regular 1-D network structure. This requirement is imposed by the requirement of PNC, and it does not exist in the setting in [107], which considers SNC only.

Define the length of the linear network as one unit. We divide the line evenly into N/\log(N) bins so that the length of each bin is \log(N)/N, as in [107]. As an extension, we further divide each bin into \log(N)/\log\log(N) sub-bins, and the length of each sub-bin is \log\log(N)/N. With an approach similar to that in [108], we can prove the following lemma.

---

\(^6\) Two caveats are in order. The first is that according to our construction, there could be “trivial” PNC units with two nodes only. In this case, the PNC relay mechanism is not needed, and each node gets to transmit directly to the other node. Regardless of whether the PNC unit is trivial or not, two time slots are needed for the bidirectional flows. The second caveat is that there could be two PNC units in the same dual packing next to each other. For example, suppose nodes 1, 2, and 3 form a PNC unit, and nodes 4, 5, 6 forms another. To avoid conflict, the scheduling of the transmissions on these two PNC units should be such that nodes 1, 3, 4 and 6 transmit in one time slot while nodes 2 and 5 transmits in another time slot. Again, two time slots are needed. The SIR in linear network is much larger than the threshold and the PNC schedule is feasible under the 10 dB SIR threshold [103].

\(^7\) To see this intuitively, consider that there N/2 flows. If we examine the “bottleneck” link in the middle of the 1-D network, asymptotically there are N/8 flows having traffic crossing from left to right of this bottleneck link, and N/8 flows having traffic crossing from right to left; the other N/4 flows do not have traffic crossing the bottleneck links. Thus, by the half-duplex constraint, at least N/4 time slots are needed for the traffic that crosses the bottleneck link. Therefore, there must be at least N/4 time slots within each frame.
Lemma 1. With high probability, there is at least one node in each sub-bin as $N$ goes to infinity.

We select one node in the middle sub-bin of each bin as the routing node. We can prove the following lemma.

Lemma 2. According to our sub-bin construction scheme, the distance between any two adjacent routing nodes is lower- and upper-bounded by $\log N / N [1 - \log N / \log N]$, $1 + \log N / \log N$. As $N$ goes to infinity, the upper bound and the lower bound converge. In other words, the routing nodes form a regular linear network for large $N$.

The transmission schedule is divided into two phases as in [107]. In the first phase, the nodes in each bin transmit their own traffic to the routing node and the routing node broadcasts the received information to the nodes in the same bin with one-hop transmissions. In the second phase, the transmission scheme for the regular 1-D network is adopted by all the routing nodes for the transport of inter-bin traffic.

We first argue that the time used for the first phase is of order $\log(N)$ with high probability. Using the Chernoff Bound, the probability that the number of nodes in each bin is more than $\log(N)$ can be shown to be less than $1/N$. Therefore, the probability that the bin with maximum nodes has more than $2 \log(N)$ nodes is less than $\frac{1}{\log(N)}$. By noting that the time of the first phase is negligible compared with the time used in the second phase, we can prove the following theorem by focusing on the time used for the second phase.

Theorem 2. With PNC, we can approach the upper bound of the per-flow throughput of the 1-D random network with high probability:

$$
\lambda_{\text{PNC}}(N) = \frac{4}{N/\log(N)} - \frac{O(1/\log(N) / \log(N))}{\log(N)}
$$

We will not go into the details of the proof of Theorem 2. The proof approach is as follows. We divide the $N/2$ flows randomly into $\lfloor \log(N) \rfloor$ groups, with each group having $K = N / (2 \log(N)) \leq \lfloor N / (2 \log(N)) \rfloor$ flows. We then apply Theorem 1’ by setting $N$ in Theorem 1’ to $2K$. Application of Theorem 1’ on all the $\lfloor \log(N) \rfloor$ groups yields the above result.

Topology 3: regular 2-D network

We now extend the regular 1-D results to the regular 2-D case as shown in Fig. 23, where $N$ nodes are uniformly located at the cross points of the grid network. To ensure that the SIR is above a target threshold, the transmissions in the horizontal lines and vertical lines can be performed in orthogonal time slots. Consider the horizontal lines (similar schedule applies for the vertical lines). The first two time slots are dedicated to transmissions on lines $1, J + 2, J + 4, \ldots$; the next two time slots are dedicated to transmissions on lines $2, J + 2, J + 4, \ldots$; and so on. The separation $J$ must be large enough to meet the target SIR requirement. As shown in [103], for a typical value of $\alpha = 4$, the SIR is about 13.5 dB, 12.3 dB, and 10.0 dB for $J = 5, 4, 3$ respectively. With an assumed 10 dB target, $J = 3$ is enough to guarantee successful transmissions.

Let us now investigate the application of PNC in the 2-D grid network with a more general traffic pattern. Here we apply a simple routing scheme, as in [107]. For a source–destination pair $(x_s, y_s) - (x_d, y_d)$, the data will be first forwarded vertically to the node at $(x_s, y_d)$ before being forwarded horizontally to the destination $(x_d, y_d)$. The horizontal and vertical transmissions are separated into two different time intervals. For horizontal (or vertical) transmissions, the scheduling within each row (column) is the same as that in 1-D topology and the scheduling among different rows (columns) is the same as above.

Consider the horizontal transmission. We argue that the number of flows in each row is almost bounded to the average value $\sqrt{N}/2$ with high probability as $N$ goes to infinity. The sketch of the argument is as follows. Using the Chernoff Bound and based on the assumption of random source/destination selection procedure, we can prove that...
the number of sources is almost equal to the number of
destinations in each row (or column), both of which
are bounded as $\sqrt{N}(0.5 - \log(\sqrt{N})/\sqrt{N} + 0.5 + \log(\sqrt{N})/\sqrt{N})$ with
probability more than $1 - 1/N$. Then, it can be proved
that the maximum number of source/destination nodes
in any of the $\sqrt{N}$ lines is less than $\sqrt{N}(0.5 + \log(\sqrt{N})/\sqrt{N})$
with probability $1 - 1/\sqrt{N}$, which goes to 1 as $N$ goes
to infinity. According to the result in Theorem 1, the
per-flow PNC throughput is four times the reciprocal of
the number of nodes within the row (or column), $4/\sqrt{N}$, with high probability. Since the horizontal transmissions
and vertical transmissions are scheduled in different time
intervals and in each interval every $j$ lines (columns) transmit simultaneously, we have

**Theorem 3.** With PNC, and with the source and destination
nodes randomly selected from the $N$ nodes with equal
probability, the per-flow throughput of the 2-D grid network
can approach the following for large $N$ with high probability:

$$\lambda_{\text{PNC}}(N) = \frac{4}{\sqrt{N}} \cdot \frac{1}{j} = \frac{2}{j\sqrt{N}}$$  \hspace{1cm} (44)

where $j$ is determined by the SIR threshold. A typical value of $j$
is 3 (under an SIR threshold of 10 dB and path-loss exponent
of 4).

**Topology 4: random 2-D network**

The idea behind the analysis of the random 2-D network
is similar to that of the random 1-D network. We first
divide the region into small grids of size $\log\sqrt{N}/\sqrt{N}$ and
then divide each small grid into subgrids of size

$$\frac{\log\sqrt{N}/\sqrt{N}}{\log\sqrt{N}/\sqrt{N}}$$

We then select one node in the middle subgrid as
a routing node and we can prove that all the routing nodes
form a regular 2-D network asymptotically.

The transmission is divided into two phases. The first
phase is dedicated to the local transmission within each
small grid, where one-hop transmissions are adopted. The second phase is dedicated to the transmission among
routings nodes, which uses the strategy as discussed in the
2-D regular network. As with the random 1-D network,
it can be proved that the time used for the first phase is
negligible compared with that used in the second phase.
The set-up in the second phase is such that it is equivalent
to a regular 2-D network with $\sqrt{N}/\log\sqrt{N} \times \sqrt{N}/\log\sqrt{N}$ nodes and
$N/2$ flows in total. Similar to the argument in Theorem 1,
we randomly divide all the flows into $[\log^2\sqrt{N}]$ groups
and the traffic of the flows are transmitted group by group.
Then we have the following theorem.

**Theorem 4.** With PNC, and with the source and destination
nodes randomly selected from the $N$ nodes with equal
probability, the per-flow throughput of the 2-D random
network can approach the following for large $N$ with high probability:

$$\lambda_{\text{PNC}}(N) = \frac{4}{\sqrt{N}} \cdot \frac{1}{j} = \frac{2}{j\sqrt{N}}$$  \hspace{1cm} (45)

where $j$ is determined by the SIR threshold. A typical value of $j$
is 3 (under an SIR threshold of 10 dB and path-loss exponent
of 4).

We remark that the result that $\lambda_{\text{PNC}}(N) = \Theta(1/\sqrt{N})$ in
Theorem 4 is consistent with the prior results on the non-
PNC system making use of the traditional multihopping
technique. The seminal paper [105] established that the
throughput per flow in the traditional wireless network subject
to SIR constraint is $\Omega(1/\sqrt{N})$. The paper, however,
only demonstrated that throughput of $\Omega(1/\sqrt{N\log N})$
is achievable when the sources and destinations are
randomly placed. The gap between the upper bound
and lower bound was closed by [106], which provides a
hierarchical routing scheme (the hierarchical scheme we
assume here is similar in spirit to that scheme although not
exactly the same) that can achieve $\Omega(1/\sqrt{N})$ throughput.
Thus, the throughput per flow is also $\Theta(1/\sqrt{N})$ in the
traditional wireless network. The advantage of PNC lies
in the smaller constant factor to $1/\sqrt{N}$ rather than order
improvement.

5.2. Practical protocol design

The transmission strategy in Section 5.1 provides
much insight on the application of PNC in wireless
networks. For example, selecting the routing nodes (relays)
for forwarding is analogous to the hierarchical routing
strategy in mesh networking in which cluster heads are
responsible for forwarding traffic between different
clusters of nodes.

The centralized TDMA MAC protocol in Section 5.1,
however, may not be practical in two settings. First, when
the number of nodes $N$ is large, the complexity of cen-
tralized routing and scheduling may become unmanageable.
Second, in many practical scenarios, the traffic from the
flows is not constant and may be bursty in nature.

In this section, we consider a distributed MAC similar
to that in IEEE 802.11 to coordinate transmissions in a
distributed manner. We borrow the protocol ideas in [109]
and the synchronization ideas in [16] to present an
opportunistic protocol based on 802.11 for applying PNC in
WiFi access network.

Consider the simple two-hop relay network in WLAN as
shown in Fig. 24. A cluster of clients are connected to the
AP via a wireless relay. We assume that traffic may be
generated by the AP or the clients in an unpredictable manner.
Thus, the initiation of a transmission may come from the
AP or a client. To make use of PNC, whenever possible we
would like to merge two transmissions in opposing direc-
tions together into an overlapped transmission. Thus, be-
fore a node (the AP or a client) begins transmitting a full-
length DATA packet, it will send a probe in the form of an
RTS (request-to-send) to the relay to look for an opportu-
nity to merge the transmission of the DATA packet with a
DATA packet in the opposite direction.

With reference to Fig. 24, suppose that the AP and the
colored (filled) client have a packet to transmit to each
other. A sequence of events in our opportunistic protocol
is depicted in Fig. 25 and described as follows. With a MAC
Fig. 24. A relay network where a cluster of clients are connected to the AP via a relay.

Fig. 25. An opportunistic transmission protocol for PNC.

The protocol is opportunistic in that a bidirectional PNC transmission will be used only when there is an opportunity to do so. If only the AP has a packet for the target client, ordinary one-way transmission will be adopted.

The protocol could be further improved by allowing a different client in the same cluster to transmit to the AP while the AP transmits to its target client. That is, if the AP’s target client, say client A, does not have a packet for the AP, but a different client within the overhearing range of the client A, say client B, has a packet for the AP, then client B can also try to combine its transmission with the transmission of the AP to the relay. In this case, in the third transaction in Fig. 25, it is client B that transmits its data to the relay. This transmission can be overheard by client A and becomes its “self-information”. Then, when the relay transmits the NC data to client A, client A can decode it. This feature requires the clients within the region to be able to overhear each other so that they can learn about each other’s self-information. There are also details to work out, including the possibility of two clients having packets to the AP. The coordination is an interesting topic for future research.

5.3. To probe further

The asymptotic performance of PNC in large 2-D wireless networks under random unicast traffic was given in [104]. Unlike our treatment here which assumes the more realistic physical interference model for the PNC analysis, the pairwise protocol interference model was assumed in [104].

In [111], the physical interference model was adopted with a highway system as in [106]. The highway system we consider in this paper is slightly different in that the routing nodes (nodes in the highway) form a 2-D regular network while that in [106] is not regular. The asymptotic throughput per flow obtained in [111] is somewhat inferior to what we have here, although they are of the same order.

In [112], the broadcast setting is analyzed for 2-D regular networks. Specifically, the times needed to broadcast blocks of data from one source node to all other nodes in the 2-D grid and hexagonal networks were analyzed, and broadcast throughput with PNC is 2.5 times that the traditional multihop scheme in the grid network, and 2 times in the hexagonal network. The result also implies that PNC can approach the broadcast throughput upper bound under the half-duplex constraint in which a node...
can be transmitting at most half the time when relaying the broadcast information.

Ref. [113] studied the scheduling problem in Analog Network Coding systems assuming the physical interference model. As with the scheduling problems in non-network-coded systems, scheduling remains a difficult problem in network-coded system. NP-completeness proofs were given in [113].

Ref. [114] formulated an optimization problem to solve the scheduling problem in PNC relay networks, assuming unicast traffic. Formulation in a multichannel network and the scheduling problem in PNC relay networks, assuming proofswere given in [113].

Ref. [116] proposed a scheme for ANC relaying that makes use of the RTS/CTS mechanism to coordinate the simultaneous transmissions of two nodes to the relay. For ANC, the channel state information \(h_{1R}, h_{2R}, h_{R1}, h_{R2}\) are needed for signal processing at the two end nodes. The paper proposed to carry this information in stages within the RTS, CTS, and ACK frames sent during the handshake process. In PNC systems in which the processing at the relay also requires the channel state information, similar ideas of piggy-backing the channel information on the control frames are also possible. An essence is to perform channel estimation using control frames that are not sent simultaneously by the two end nodes. Channel estimation based on simultaneous received packets is challenging in practice and is still a rather open communication-theoretic research problem as far as we know.

6. Optical PNC

PNC was originally proposed for application in wireless networks. It is based on the observation that network coding operation is implicit in many natural phenomena. Whenever two quantities in nature, \(x\) and \(y\), meet to produce a third quantity, \(z = f(x, y)\), a form of network coding operation occurs. For example, \(z\) could be the amplitude of an EM wave when \(x\) and \(y\) are amplitudes of coherent EM waves; or \(z\) could be sum power of two EM waves when \(x\) and \(y\) are the powers of noncoherent EM waves. In general, \(x\) and \(y\) could be other physical quantities, including acoustic waves.

We end this paper by proposing to apply PNC in the optical domain. Since light is also a form of EM wave, PNC for lightwave communication is just a small step from PNC for wireless communication. For fiber-optic communication, the channel gain is more stable and the issue of fading is not a main concern. Also, full duplexity can be more readily implemented by isolating the transmitted signal from the received signal through two different optical fibers, or on the same fiber through a directional coupler at the transceiver. Conceivably, it could even be easier to realize PNC in fiber-optic communication than in wireless communication, especially for noncoherent optical systems. We provide an example of optical PNC in this section.

The passive optical network (PON) [117] is a network architecture of much interest in the optical communication community. PONs have also been commercially deployed in the field. A PON consists of an optical line terminal (OLT) at the central office, a passive optical splitter–combiner, and a number of optical network units (ONUs) at or near the end users’ premises. Downstream signals are broadcasted by the OLT to the ONU, and each ONU filters out all the signals except its own signal; encryption can be used at the upper layer to prevent eavesdropping. Upstream signals from the ONUs to the OLT make use of a multiple access protocol for access of the shared medium. The time-division-multiple-access (TDMA) protocol is popular protocol being used.

For generality, we consider here the star topology as shown in Fig. 26. Here, node 1 could be the OLT, and nodes 2 to \(N\) could be the ONUs. More generally, for our purpose here, we do not assign specific roles to the nodes. We simply have a system in which there are \(N\) nodes wanting to exchange information with each other. Each node is connected to the splitter-combiner through an output fiber and an input fiber. In principle, the input and output fibers could also be the same physical fiber with signals traveling in opposite direction; a directional coupler is inserted at a node to isolate the transmitted and received signals.

At the splitter-combiner, the signals from its inputs are combined and broadcasted to all the nodes. For example, if node 1 sends \(S_1\) and node 2 sends \(S_2\), all the nodes receive \(S_1 + S_2\). We see immediately that PNC has a role to play here. In particular, it allows full-duplex communication between two nodes in the network at any given time. Suppose that \(S_1\) is targeted for node 2, and \(S_2\) is targeted for node 1. With the pure TDMA system, nodes 1 and 2 will send \(S_1\) and \(S_2\) in two different time slots. With PNC, nodes 1 and 2 will send \(S_1\) and \(S_2\) together, and they use self-information to extract \(S_2\) and \(S_1\), respectively, from \(S_1 + S_2\). The potential throughput increase, as in wireless, is 100%.

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8 In the single-fiber system, each node is connected only to an input of the splitter–combiner (star coupler). A loop-back path is set up by interconnecting two outputs of the splitter–combiner, say outputs 1 and 2. The signal on one output is looped back from the other output for broadcast to all the inputs of the splitter-combiner. In this way, the transmitted and received signals of a node travel on the same fiber in opposite directions. The single-fiber system incurs signal attenuation of \(1/N^2\) while the double-fiber system incurs attenuation of \(1/N\) at the splitter–combiner.
Compared with wireless communication, a subtlety is as follows. In wireless communication, half-duplex constraint is often imposed. This is because the signal being transmitted is of much higher power than the signal being received if simultaneous transmission and reception are allowed, and it is not easy to extract the received signal in practice. For the optical star, the transmitted signal at a node is isolated from the received signal through two different optical fibers (or a directional coupler on a single fiber). For node 1, in the received composite signal $S_1 + S_2$, the power of $S_1$ may not be much larger than that of $S_2$. This makes it easier to implement a full-duplex system in the optical star network.

When the traffic is bursty and unpredictable, the use of TDMA is not efficient. A random multiple-access protocol (e.g., carrier-sense-multi-access) can be used to coordinate the access of the shared medium among the nodes. A MAC protocol for bidirectional communication that employs PNC can be as follows. Suppose that node 1 acquires the channel and sends a burst of data to node 2, and this burst triggers a burst of data from node 2 to node 1 in the reverse direction (many real-world applications are bidirectional in that when there is data in one direction, there is also data in the reverse direction at the same time). Without PNC, the two bursts must acquire the channel separately using the random multiple-access protocol. With PNC, once node 1 acquires the shared medium and sends a data burst to node 2, node 2 will detect that it is the recipient of the data; and if node 2 also has data for node 1, it can simultaneously send the data burst to node 1. Thus, channel acquisition is bidirectional.

The observant reader may notice wavelength-division-multiple-access (WDMA) could achieve the same effect. Specifically, the signal from node 1 to node 2 and the signal from node 2 to node 1 can be carried on two different wavelengths. Thus, simultaneous bidirectional communication is also possible with WDMA. However, if multiple wavelengths were available, PNC could still achieve better throughput. Instead of using the two wavelengths for one bidirectional flow, the two wavelengths could be used for two bidirectional flows, hence doubling the throughput. To see this in a concrete way, let us look at Fig. 26 again. For simplicity, suppose that there are only four nodes so that $N = 4$. Further suppose that there are two available wavelengths $\lambda_a$ and $\lambda_b$. Without using PNC, only two simultaneous flows can be supported. For example, we could use $\lambda_a$ to support a flow from node 1 to node 2, and $\lambda_b$ to support a flow from node 2 to node 1. Although nodes 1 and 2 will receive both signals, a wavelength filter can be used to separate out the desired wavelength. With PNC, we could just use one wavelength, say $\lambda_a$, to simultaneously support the flow from node 1 to node 2 and the flow from node 2 to node 1. Instead of using a wavelength filter to extract the desired signal, we cancel out the self-information in the electronic domain only after reception. Thus, there is also a bidirectional flow between nodes 3 and 4, we could use $\lambda_b$ and the PNC technique to support it. In this way, the use of PNC can double the throughput of the system. For general $N$, when the number of wavelengths is smaller or equal to $N/2$, the throughput can be doubled with PNC in the above manner.

While there have been many works on wireless PNC since [1], to our knowledge, there has not been any work on optical PNC. This is a first proposal suggesting that PNC can be extended to the optical domain. We have considered a rather simple optical network. There could be other optical scenarios in which PNC is useful. The optical domain appears to be a fertile ground for future PNC research.

7. Conclusions

We have introduced PNC and overviewed some recent research results. The recent works are categorized into three domains: (1) wireless communication, (2) information theory, and (3) wireless networking. Within the three domains, we have further grouped works into various sub-domains. We believe researchers in the field will find our survey and categorization useful as a reference in their future investigations. Despite our attempts to list and categorize the major works, it is likely that we have also missed some important works, especially the more recent ones.

To date, most works on PNC have focused on two-way relay channel (TWRC). The theoretical understanding of TWRC is maturing. An unresolved issue is the information-capacity region of TWRC. The use of multiuser detection (MUD) technique could approach the capacity at the low SNR regime, and the use of nested lattice code and the corresponding detection technique could approach the capacity at the high SNR regime. Neither technique, however, gives the ultimate information capacity of PNC TWRC for all SNR. As outstanding challenge is the information capacity of TWRC and an efficient implementation to achieve it.

Beyond TWRC, there have also been many investigations on its extension to the multi-way relay channel (MWRC) in which a relay (or a system of relays) interconnect more than two end nodes. We believe the theoretical understanding of MWRC will also be maturing shortly.

In both TWRC and MWRC, there are at most two hops between two communicating end nodes. In a general multihop network, MAC-layer and network-layer issues
will take on an increasingly important role, particularly with regard to complexity management when there are many simultaneous flows in the network. We have outlined the potential use of the concept of virtual paths in PNC to manage complexity at the network layer. We have also briefly discussed MAC-level issues by means of an MAC scheduling protocol. By and large, these have been high-level discussions and many details remain to be ironed out. Compared with the large volumes of communication-theoretic and information-theoretic PNC investigations, there have been far fewer works with a networking flavor. A reason could be that the problem formulations at the MAC and network layer are not as clear-cut as those at the lower layers. There are many outstanding challenges at the higher layers.

Another fertile ground for future PNC research is implementation and prototyping. Besides [6,22], we are not aware of other successful implementations of PNC. There is a gap between theory and implementation at the moment. We believe that beyond the implementations of [6,22], PNC systems with better performance could be demonstrated, and worthwhile issues for further theoretical and experimental investigations could be identified through such prototyping efforts.

Finally, although PNC was originally conceived for application in wireless networks, network coding operations abound in nature. In fact, any physical phenomenon in which an effect (output) is the outcome (function) of a number of causes (inputs) can be exploited in the network coding construct. In this paper, we have attempted to extend the application of PNC to optical networks. The application of PNC could potentially be extended to many other domains.

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Appendix. System model and notation

Much of this document focuses on the application of PNC in TWRC. In this appendix, we formally define the system model and the notation used. Fig. A.1(a) depicts a TWRC, in which nodes 1 and 2 exchange information with the help of relay node R. We assume that all nodes are half-duplex, i.e., a node cannot receive and transmit simultaneously. We also assume that there is no direct link between nodes 1 and 2. An example in practice is a satellite communication system in which the two end nodes on the earth can only communicate with each other via the relay satellite.

Fig. A.1(b) is a schematic diagram of our system which includes the possibility of channel coding on top of physical-layer network coding. This paper adopts the following notation. In general, we use upper letters to denote packets and lower letters to denote symbols within packets.

- \( N \) is the number of symbols in a channel-coded packet.
- \( M \leq N \) is the number of symbols in a source packet.
- \( S_i = (s_i[1], s_i[2], \ldots, s_i[M]) \) denotes the source packet of node \( i \), \( i \in [1, 2] \).
- \( X_i = (x_i[1], x_i[2], \ldots, x_i[N]) \) denotes the channel coded packet of node \( i \), \( i \in [1, 2] \).
- In non-channel-coded PNC, \( S_i = X_i \) and \( M = N \).
- \( Y_R = (y_R[1], y_R[2], \ldots, y_R[N], y_R[N + 1], \ldots, y_R[2N + 1]) \) denotes the received packet at relay node R. Note that here we assume this is an offset \( \Delta \) between the symbols of nodes 1 and 2 at the relay, and that oversampling is used to collect \( 2N + 1 \) samples from the simultaneously received packets. If there is no symbol offset, then only \( N \) samples will be collected. See Section 3.1.3 for details.
- \( W_R = (w_R[1], w_R[2], \ldots, w_R[N], w_R[N + 1], \ldots, w_R[2N + 1]) \) denotes the receiver noise at relay R embedded in \( Y_R \).
- \( \hat{S}_R = (\hat{s}_R[1], \hat{s}_R[2], \ldots, \hat{s}_R[M]) \) denotes the network-coded source packet produced by relay \( R \) based on \( Y_R \) in non-channel-coded PNC and link-by-link channel-coded PNC. Symbol \( \hat{s}_R[m] \) is an estimate of the network-coded symbol \( s_R[m] = f(s_1[m], s_2[m]) \). For BPSK and QPSK, this document assumes \( \hat{s}_R[m] = s_1[m] \oplus s_2[m] \).
- \( X_R = (x_R[1], x_R[2], \ldots, x_R[N]) \) denotes the packet broadcasted by Relay R to nodes 1 and 2. In non-channel-coded PNC, \( X_R = \hat{S}_R \). In link-by-link channel-coded PNC, \( X_R \) is the channel-coded packet computed from the source packet \( \hat{S}_R \).
- \( Y_i = (y_i[1], y_i[2], \ldots, y_i[N]) \) denotes the received PNC packet at node \( i \), \( i \in [1, 2] \).
- \( W_i = (w_i[1], w_i[2], \ldots, w_i[N]) \) denotes the receiver noise at node \( i \) embedded in \( Y_i \), \( i \in [1, 2] \).
- \( \hat{S}_i = (\hat{s}_i[1], \hat{s}_i[2], \ldots, \hat{s}_i[M]) \) denotes the decoded source packet of node \( i \), \( i \in [1, 2] \), at the other end node.
For BPSK, \(s_1[.]\), \(x_1[.]\), \(s_2[.]\), \(x_2[.]\) \(\in \{-1, 1\}\).

For QPSK, \(s_1[.], x_1[.], s_2[.], x_2[.] \in \{(1 + j)/\sqrt{2}, (1 - j)/\sqrt{2}\}\)

\(1, -j)/\sqrt{2}, (1 + j)/\sqrt{2}\), and \(y_1[.], y_2[.]\)

\[w_i[.], w_j[.] \in C\].

\(b_i, i = \{1, 2\}\) denotes the channel gain from node \(i\) to relay \(R\).

\(b_i, i = \{1, 2\}\) denotes the channel gain from relay \(R\) to node \(i\).

\(\Delta \in \{0, 1\}\) denotes the symbol offset between the symbols from nodes 1 and 2 when they arrive at relay \(R\).

\(\phi\) denotes the phase offset between the carriers of nodes 1 and 2.

\[R_1 = \frac{1}{\sqrt{2}} \sum_{i=1}^{2} (s_i + x_i)\]

\(\sqrt{2} s_i, \sqrt{2} x_i, \sqrt{2} y_i, \sqrt{2} w_{ij}\).

\(\hat{s}_i, \hat{x}_i\)

\[\Gamma = \frac{1}{\sqrt{2}} \sum_{i=1}^{2} (s_i + x_i) - \frac{1}{\sqrt{2}} \sum_{i=1}^{2} (s_i + x_i)\]

\[\frac{1}{\sqrt{2}} (s_i + x_i - s_j - x_j)\]

\(\sqrt{2} (s_1 + x_1 - s_2 - x_2)\).

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Soung Chang Liew received his S.B., S.M., E.E., and Ph.D. Degrees from the Massachusetts Institute of Technology. From 1984 to 1988, he was at the MIT Laboratory for Information and Decision Systems, where he investigated Fiber-Optic Communications Networks. From March 1988 to July 1993, he was at Bellcore (now Telcordia), New Jersey, where he engaged in Broadband Network Research. He has been Professor at the Department of Information Engineering, the Chinese University of Hong Kong, since 1993. He is Adjunct Professor at Southeast University, China.

Shengli Zhang received his B.Eng. Degree in electronic engineering and the M.Eng. Degree in communication and information engineering from the University of Science and Technology of China (USTC), Hefei, China, in 2002 and 2005, respectively. He received the Ph.D. Degree from the Department of Information Engineering, the Chinese University of Hong Kong (CUHK), in 2008. From 2002 to 2005, he was with the Personal Communication Network and Spread Spectrum (PCN & SS) Laboratory, USTC, as a Research Engineer involved in several National 863 Research Projects including the Beyond-3 Generation of Mobile System in China (FUTURE Plan). From 2002 to 2005, he was also a Research Engineer of the USTStarcom Wireless Soft Research Center, Hefei, China, involved in the research and implementation of the WCDMA communication systems. From Oct. 2008, he was a Research Associate at CUHK. He is an assistant professor with the Communication Engineering Department, Shenzhen University, China. His current research interests include wireless networks, wireless communication, physical layer network coding, and cooperative wireless networks.

Lu Lu (S’10) received his B.E. Degree in Electronic Engineering and Information Science from the University of Science and Technology of China (USTC), Hefei, China, in 2007, and his Ph.D. Degree in Information Engineering from The Chinese University of Hong Kong (CUHK), Hong Kong, in 2012. He is now a postdoctoral fellow with the Institute of Network Coding and the Department of Information Engineering, CUHK. His current research interests include wireless communication in 802.11 networks, multi-user detection, collision resolution, physical-layer network coding and software-defined radios.