Elevation Angle-Dependent 3D Trajectory Design for Aerial RIS-Aided Communication
Yifan Liu, Bin Duo, Qingqing Wu, Xiaojun Yuan, Jun Li, and Yonghui Li

Abstract—This paper investigates an aerial reconfigurable intelligent surface (RIS)-aided communication system under the probabilistic line-of-sight (LoS) channel, where an unmanned aerial vehicle (UAV) equipped with an RIS is deployed to assist two ground nodes in their information exchange. An optimization problem with the objective of maximizing the minimum average achievable rate is formulated to jointly design the communication scheduling, the RIS’s phase shift, and the three-dimensional (3D) UAV trajectory. To solve such a non-convex problem, we propose an efficient iterative algorithm to obtain its suboptimal solution. Simulation results show that our proposed design significantly outperforms the existing schemes and provides new insights into the elevation angle and distance trade-off for the UAV-borne RIS communication system.

Index Terms—UAV communication, reconfigurable intelligent surface, probabilistic LoS channel, trajectory design.

I. INTRODUCTION

BESIDES terrestrial deployment, wireless networks are gradually evolving into air-ground integrated networks to achieve ubiquitous wireless connection and network capacity upgrades [1], [2]. Recently, unmanned aerial vehicles (UAVs) have obtained substantial attention in wireless communication. Thanks to their high mobility, low cost, and line-of-sight (LoS) transmission, UAVs can further improve communication coverage, throughput, and average secrecy rates [3], [4], [5].

Recently, the reconfigurable intelligent surface (RIS) has attracted considerable attention due to its low profile, low energy consumption, and ability to overcome the non-LoS (NLoS) transmission [6]. Typically, the RIS contains many reflective elements, each of which is manipulated to induce changes in the amplitude and phase shift of incident signals to create favorable propagation environment. The RIS becomes a promising technology for the future mobile communications. It can solve the pain points of fifth-generation (5G) communications. It can solve, since it contains intractable non-convex constraints, binary

For typical application scenarios of UAV communications in urban areas, such as cargo delivery, traffic monitoring, and so on, their communication links are often blocked by tall building, which leads to severe degradation of channel quality. Fortunately, with its low power consumption and lightweight, the RIS can be installed at an appropriate location to reconfigure the propagation environment of air-ground links, thereby improving communication performance. Several works have studied various RIS-assisted UAV communication systems. In general, these studies mainly fall into two categories, one for terrestrial RIS [8], [9], [10], [11], [12] and the other for aerial RIS [13], [14], [15], [16], [17], [18]. In particular, for the first category, the UAV trajectory and the phase shift of the RIS mounted on building facades are jointly designed to optimize different objectives such as communication coverage [8], energy efficiency [9], confidentiality [10], [11], and communication rates [12].

Taking advantage of the UAV’s ability to fly freely in the three-dimensional (3D) space, the RIS can be mounted on the UAV. This allows the RIS to fly along with the UAV, which is more flexible in adjusting its 3D location than the conventional terrestrial RIS, thus enhancing communication services [13], [14]. An aerial RIS was deployed in [15] to expand the coverage of communication services, where the worst-case signal-to-noise ratio (SNR) was improved by jointly optimizing the transmit beamforming, the RIS’s placement, and the 3D passive beamforming. In [16], multiple users were served by a base station (BS), and their received powers were significantly enhanced with the aid of an aerial RIS. To provide communication services for blocked users that locate far apart while preventing information leakage, the UAV equipped with one RIS was deployed in [17] to improve the security and energy efficiency. In [18], the authors proposed a covert communication scheme assisted by the aerial RIS, where the covert transmission rate was improved by alternatingly optimizing the transmit power of Alice, the RIS phase shift, and the horizontal location of the UAV. Above works only took the ideal deterministic LoS channel (DLC) into account, which has two limitations in practice. i) The DLC model cannot fully capture the critical effects of the UAV location-dependent LoS and NLoS states in urban areas with typically high and dense buildings/trees [19]; ii) the DLC model cannot accurately describe the elevation angle and distance trade-off, since the elevation angles between the UAV and ground nodes (GNs) are closely related to the 3D UAV trajectory [20]. Therefore, it is intuitive that the UAV trajectory designed under the simplified DLC model will undoubtedly cause significant performance loss in practical urban environments.

Motivated by the above, this paper considers an aerial RIS-aided communication system, where the UAV-borne RIS assists in information exchange with two GNs. In particular, we adopt a more accurate probabilistic LoS channel (PLC) model to characterize the complex channel states of LoS and NLoS in an urban environment. To maximize the minimum average achievable rate, we jointly optimize the communication scheduling, the RISs phase shift, and the 3D UAV trajectory. The formulated problem is non-convex and difficult to solve, since it contains intractable non-convex constraints, binary

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scheduling variables, and the complicated achievable rate expression concerning UAV trajectory variables. To tackle such challenges, we propose an efficient iterative algorithm to obtain a high-quality solution. Simulation results show that our proposed joint design for the aerial RIS-aided communication system under the PLC model can significantly improve the max-min rate compared to that under the conventional DLC model. This is because the optimized UAV trajectory better balances the elevation angle and distance trade-off, resulting in the enhanced gain of the cascaded channel between the UAV and the GNs.

Note that although the authors in [21] and [22] also considered a UAV-borne RIS communication system under the PLC model, in this paper, both the system model and the proposed algorithm are different, which results in the fundamental trade-off between the elevation angle and distance for rate enhancement.

II. SYSTEM MODEL AND PROBLEM FORMULATION

In this paper, we consider an aerial RIS-aided communication system, where two GNs exchange information via a UAV-borne RIS due to the blockage of dense buildings. We characterize the position of the UAV and the two GNs via the 3D Cartesian coordinate system. It is assumed that the UAV flies over a given duration $T$ to assist in reflecting signals via the RIS between the GNs, whose locations are denoted by $w_k = [x_k, y_k]$, $k \in K = \{1, 2\}$. To ease the 3D UAV trajectory design, $T$ is divided into $N$ equal time slots, where $\delta_t$ is the length of each time slot. Thus, the trajectory of the UAV can be approximated by a 3D sequence $\{\mathbf{q}[n], h[n]\}$, $n \in N = \{1, 2, \ldots, N\}$, where the discrete waypoints $\mathbf{q}[n] = [x[n], y[n]]$ and $h[n]$ represent the horizontal and vertical locations, which satisfy the following constraints:

$$\|\mathbf{q}[n+1] - \mathbf{q}[n]\|^2 \leq \Omega^2, \forall n,$$

$$\|\mathbf{q}[N+1] - \mathbf{q}[1]\|^2 = \mathbf{q}_0,$$

$$\|h[n+1] - h[n]\|^2 \leq \Omega^2, H_{\text{min}} \leq h[n] \leq H_{\text{max}}, \forall n,$$

where $\mathbf{q}_0$ and $\mathbf{q}_F$ denote the initial and final horizontal positions of the UAV, respectively, $\Omega = \hat{v}_{\text{max}}\delta_t$ and $\hat{\Omega} = \hat{v}_{\text{max}}\delta_t$ are the maximum horizontal and vertical distance that the UAV can reach in each time slot, respectively, and $\hat{v}_{\text{max}}$ and $\hat{v}_{\text{max}}$ are the corresponding maximum horizontal and vertical flying speed of the UAV, respectively.

Furthermore, $H_{\text{min}}$ and $H_{\text{max}}$ indicate the minimum and maximum altitude that the UAV can reach at any given time. We assume that both GN 1 and GN 2 are equipped with an omni-directional single antenna. The RIS is equipped with a uniform planar array (UPA) of $M = M_x \times M_y$ ($M_x$ rows and $M_y$ columns) reflective elements, each of which can be manipulated by an embedded development board, such as Raspberry Pi 4, mounted on the UAV. Since the UAV and the RIS are assembled compactly, we assume that their 3D coordinates are identical, causing negligible performance loss due to high flying altitude of the UAV [17]. We denote $\theta[n] = \{e^{j\theta_1[n]}, e^{j\theta_2[n]}, \ldots, e^{j\theta_{M_x}[n]}\}$ as the diagonal phase-shift matrix of the RIS in the $n$th time slot, where $\theta_{m_x,m_y}[n] \in [0, 2\pi)$ is the phase shift of the $m_x$-$m_y$th column in the $n$th time slot, where $m_x \in \mathcal{X} = \{1, \ldots, M_x\}$ and $m_y \in \mathcal{Y} = \{1, \ldots, M_y\}$. Assume that the phase shift of each element is continuously controllable, which should satisfy $|e^{j\theta_{m_x,m_y}[n]}| = 1$.

In this paper, we mainly focus on designing the UAV trajectory and the phase shift of the RIS in an offline manner. Since the small-scale fading cannot be obtained before the UAV’s mission, we adopt the PLC model to characterize the channel state statistically by modeling the occurrence probabilities of the LoS or NLoS state as a function of the UAV-ground elevation angle [26]. Thus, for GN $k$, the LoS probability in the $n$th time slot is given by

$$P_k^{\text{LoS}}[n] = \frac{1}{1 + a e^{\psi_k[n] - a}},$$

where $a > 0$ and $b > 0$ are constants specified by the actual environment, and

$$\psi_k[n] = \frac{180}{\pi} \arctan\left(\frac{h[n]}{|\mathbf{q}[n] - w_k|}\right)$$

is the elevation angle from GN $k$ to the UAV in the $n$th time slot. The relevant NLoS probability can then be acquired as $P_k^{\text{NLoS}}[n] = 1 - P_k^{\text{LoS}}[n]$. The channel gain between GN $k$ and the UAV conditioned on the LoS state in the $n$th time slot can be expressed as

$$h_k^{\text{LoS}}[n] = \tau[n] \left[1, \ldots, e^{-\frac{\pi^2}{\lambda^2}(M_x-1)\sin\varphi[n] \cos\theta[n]}\right]^{\top} \otimes \left[1, \ldots, e^{-\frac{\pi^2}{\lambda^2}(M_y-1)\sin\theta[n] \sin\varphi[n]}\right]^{\top},$$

where $\tau[n] = \sqrt{\rho_0 d_k^{\text{LoS}}[n]}$, $\rho_0$ is the path loss at the reference distance of $D_0 = 1$ meter (m), $d_k[n] = \sqrt{|\mathbf{q}[n] - w_k|^2 + h[n]^2}$ is the distance from GN $k$ to the UAV in the $n$th time slot, $\alpha_1$ denotes the path loss exponent for the LoS state. Furthermore, $d$ is the antenna separation, $\lambda$ is the carrier wavelength, $\varphi_k[n]$ and $\theta_k[n]$ represent the elevation and azimuth angles in the $n$th time slot, respectively. Furthermore, $\sin\varphi_k[n] \cos\theta_k[n] = \frac{\lambda[n] - \xi_{n_k}}{\lambda[n] + \xi_{n_k}}$ and $\sin\theta_k[n] \sin\varphi_k[n] = \frac{\lambda[n] - \xi_{n_k}}{\lambda[n] + \xi_{n_k}}$. The channel gain between GN $k$ and the UAV conditioned

To determine the maximum rate performance, the amplitude and phase shift coefficients are assumed to be continuously adjustable in this paper. The obtained continuous solutions can be quantized to discrete values for practical hardware implementation. It has been demonstrated that when the resolution is greater than 3 bits, the performance degradation induced by phase shift quantization is minimal [24].

As a matter of fact, if we can obtain the instantaneous channel state information (CSI), we can determine the UAV-ground channel state, i.e., LoS or NLoS. In this case, the online design for the UAV trajectory may be an alternative solution for higher rate performance. However, due to the mobility of the UAV and the passivity of the RIS, the full instantaneous CSI between the UAV-borne RIS and GNs in real-time is quite challenging to obtain [25], which requires further investigation.

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1Note that the movement of the UAV may change the orientation of the RIS, which will cause a difference between the phase shift designed in this paper and the required phase shift in practice, resulting in performance degradation. However, it is reasonable to assume that the RIS can always remain stable in this paper, since we can employ a three-axis gimbal along with a control system including a motion sensor and an electronic control unit (ECU) to ensure that the orientation of the RIS keeps unchanged for the duration of the UAV flight [23].

2To determine the maximum rate performance, the amplitude and phase shift coefficients are assumed to be continuously adjustable in this paper. The obtained continuous solutions can be quantized to discrete values for practical hardware implementation. It has been demonstrated that when the resolution is greater than 3 bits, the performance degradation induced by phase shift quantization is minimal [24].
on the NLoS state in the nth time slot is given by
\[ h_k^N[n] = \zeta[n] h_k, \]
where \( \zeta[n] = \sqrt{\frac{P_0 d_k^{-\alpha}}{\sigma^2}}, \) \( \alpha \) denotes the path loss exponent for the NLoS state, and \( h_k \sim CN(0, 1) \) is the small-scale fading component modeled by a circularly symmetric complex Gaussian (CSCG) random variable.

Assume that GN \( k \) operates in the half-duplex mode, i.e., it can only receive or transmit in each time slot. Thus we define a binary variable that indicates whether GN \( k \) is scheduled to receive reflected signals from the UAV in the nth time slot or not, i.e., GN \( k \) receives signals from the other GN via the RIS if \( \alpha_k[n] = 1 \), and transmits otherwise. Assume that only one GN is allowed to transmit or receive signals to or from the UAV-borne RIS in the nth time slot, so we have the following scheduling constraints:
\[ \sum_{k=1}^{2} \alpha_k[n] \leq 1, \forall n \in \mathcal{N}, \]
\[ \alpha_k[n] \in [0, 1], \forall k, n. \]

In a statistical sense, the expected achievable rate in bits/second/Hertz (bps/Hz) from GN \( \bar{k} \) through the UAV to GN \( k \) in the nth time slot can be given by
\[ \mathbb{E}[R_k[n]] = P_k^L[n] R_k^L \max_{\eta} R_k^N \bar{R}_k^N[n] \]
\[ + P_k^N[n] R_k^N \bar{R}_k^N[n] + P_k^N[n] R_k^N \bar{R}_k^N[n], \]
where \( R_k^\eta[n] = \log_2 \left( 1 + \gamma_k \left( h_k^\eta[n] \right)^H \Theta[n] h_k^\eta[n] \right)^2 \), \( f, o \in \{L, N\} \) denote respectively the achievable rates at GN \( k \) conditioned on the LoS and NLoS states of the air-ground channels. Furthermore, \( \gamma_k = P_k / \sigma^2 \), where \( P_k \) is maximum transmit power of GN \( k \) and \( \sigma^2 \) is the variance of Gaussian noise at GN \( k \).

We aim to maximize the minimum average achievable rate by jointly optimizing the communication scheduling \( A \), the horizontal UAV trajectory \( Q \), the vertical UAV trajectory \( H \), and the RIS’s phase shift \( \Theta \) for the entire \( N \) time slots. Define \( \eta \) as the minimum average expectation of the achievable rate among all users. The optimization problem can be formulated as
\[ \max_{A, Q, \Theta, H, \Phi_k, \eta} \eta \]
\[ \text{s.t. } \frac{1}{N} \sum_{n=1}^{N} \alpha_k[n] \mathbb{E}[R_k[n]] \geq \eta, \forall k \in \mathcal{K}, \]
\[ |e^{j\beta_k[n]}| = 1, \forall n, \]
\[ (1) - (3), (5), (8) - (9). \]

Problem (11) is non-convex because the rate function \( \bar{R}_k[n] \) in (11b) is not jointly concave with respect to \( A, \Theta, Q, \) and \( H \), the binary scheduling constraints in (9) are non-convex, the phase shift constraints in (11c) are non-convex, and the elevation angle constraints in (5) are non-affine, which make it difficult to obtain the optimal solution. In fact, problem (11) can be classified as a mixed-integer non-linear program (MINLP) problem and there are generally no efficient methods for solving it optimally. In the following section, we propose an efficient iteration algorithm to solve problem (11).

III. PROPOSED ALGORITHM
In this section, an alternating optimization method is proposed to obtain a high-quality solution to problem (11), where \( A, \Theta, Q, \) and \( H \) are iteratively optimized. Specifically, the original problem is partitioned into four subproblems, each of which is solved in an iterative manner until the algorithm converges. In practice, the optimization algorithm can be executed on a ground control center, which first runs the proposed algorithm and then transmits the optimized variables to the UAV via a control and non-payload communication (CNPC) link for mission execution along the designed trajectory [27].

A. GNs’ Scheduling Optimization
With any given feasible \( Q, \Theta, \) and \( H \), this subproblem can be effectively tackled by relaxing the binary variables \( \alpha_k[n] \in [0, 1] \) to continuous variables \( 0 \leq \alpha_k[n] \leq 1 \), which yields the following relaxed problem expressed as
\[ \max_{\lambda, \eta} \eta \]
\[ \text{s.t. } 0 \leq \alpha_k[n] \leq 1, \forall k, n. \]

Since problem (12) is a standard linear program, it can be solved efficiently by CVX [28].

B. RIS’s Phase Shift Design
With any given feasible \( A, Q, \) and \( H \), problem (11a) can be rewritten as
\[ \max_{\Theta, \eta} \eta \]
\[ \text{s.t. } (11b) - (11c). \]

Since the constraints (11c) are unit modulus, it is difficult to solve problem (13). To overcome this difficulty, we employ the semidefinite relaxation (SDR). To begin, let us perform the following transformation:
\[ \left( h_k^\eta[n] \right)^H \Theta[n] h_k^\eta[n] = \left( h_k^\eta[n] \right)^H \text{diag}(h_k^\eta[n]) \text{diag}(h_k^\eta[n])^T \]
\[ = \left( h_k^\eta[n] \right)^H \text{diag}(h_k^\eta[n]) \psi[n], f, o \in \{L, N\}, \]
where \( \psi[n] = [e^{j\beta_1[n]}, e^{j\beta_2[n]}], \ldots, e^{j\beta_M[n]}]^T \). According to (14), we can reinterpret the square term in the expected achievable rate as
\[ \left( h_k^\eta[n] \right)^H \Theta[n] h_k^\eta[n] \]
\[ = \text{diag}(h_k^\eta[n]) \text{diag}(h_k^\eta[n])^T \]
\[ = \text{diag}(h_k^\eta[n]) \text{diag}(h_k^\eta[n])^T \text{diag}(h_k^\eta[n]) \]
\[ = \text{diag}(h_k^\eta[n]) \text{diag}(h_k^\eta[n])^T \text{diag}(h_k^\eta[n]). \]

Then, the expected achievable rate can be re-expressed as
\[ \mathbb{E}[\bar{R}_k[n]] = P_k^L[n] P_k^L[n] \log_2 \left( 1 + \text{Tr}(V[n] G_k^{LL}[n]) \right) \]
\[ + P_k^N[n] P_k^N[n] \log_2 \left( 1 + \text{Tr}(V[n] G_k^{LN}[n]) \right), \]
\[ + P_k^N[n] P_k^N[n] \log_2 \left( 1 + \text{Tr}(V[n] G_k^{NL}[n]) \right) \]
\[ + P_k^N[n] P_k^N[n] \log_2 \left( 1 + \text{Tr}(V[n] G_k^{NN}[n]) \right). \]

Since the expected achievable rate is a function of the newly introduced variable \( V[n] \), we can alleviate the difficulties associated with using \( \psi[n] \) as the optimization variable. In this respect,
\[|v_{m,m}[n]| = 1\] can be rewritten as \(V[n] \geq 0\) and \(V_{m,m}[n] = 1\) for the new optimization variable \(V[n]\). Thus, problem (13) can be rewritten as
\[
\max_{\theta, \eta} \eta
\]
s.t. \(\frac{1}{N} \sum_{n=1}^{N} \alpha_k[n] E[H_k[n]] \geq \eta, \forall k \in K,\) \hfill (17a)
\(V[n] \geq 0,\) \hfill (17b)
\(V_{m,m}[n] = 1, m = 1, 2, \ldots, M.\) \hfill (17c)

As problem (17) is a semidefinite programming, it can be solved efficiently by CVX. However, a rank-one solution may not be obtained. Hence, we recover \(v[n]\) from \(V[n]\) using the Gaussian randomization method, which is similar to that in [10] and thus omitted here for brevity.

**C. UAV Horizontal Trajectory Optimization**

With any feasible \(H\) and \(A\) and \(\theta\) obtained by solving problem (12) and (17), respectively, the UAV horizontal trajectory optimization problem can be written as
\[
\max_{Q, \psi_k, \eta} \eta
\]
s.t. \((1) - (2), (5), (11b).\) \hfill (18)

To facilitate the solution to problem (18), we firstly rewrite Eq. (6) as \(H_k[n] = \tau[n]H_k[n]\).

\[\text{Note that not only } \tau[n] \text{ but also } H_k[n] \text{ is relevant to the UAV trajectory. It is observed that } H_k[n] \text{ is complex and non-linear with respect to the UAV trajectory variables, which makes the UAV trajectory design intractable. To handle such difficulty, we use the UAV trajectory of the } (l - 1) \text{ th iteration to obtain an approximate } H_k[n] \text{ in the } l \text{ th iteration [10]. Therefore, constraint (11b) can be re-expressed as}
\]
\[
\frac{1}{N} \sum_{n=1}^{N} \alpha_k[n] \left( P^L_k[n]P^L_k[n] \log_2 \left( 1 + \frac{\xi_k^{LL}[n]}{\alpha_k[n]^2} \right) + P^L_k[n]P^N_k[n] \log_2 \left( 1 + \frac{\xi_k^{LN}[n]}{\alpha_k[n]^2} \right) + P^N_k[n]P^N_k[n] \log_2 \left( 1 + \frac{\xi_k^{NN}[n]}{\alpha_k[n]^2} \right) \right) \geq \eta.
\]
where
\[
\xi_k^{LL}[n] = \frac{p_k^L[r_0^2]}{\sigma^2} \left( H_k[n]H_k[n]^H \right) \Theta [\alpha_k[n]^2],
\]
\[
\xi_k^{LN}[n] = \frac{p_k^L[r_0^2]}{\sigma^2} \left( H_k[n]H_k[n]^H \right) \Theta [\alpha_k[n]^2],
\]
\[
\xi_k^{NL}[n] = \frac{p_k^L[r_0^2]}{\sigma^2} \left( H_k[n]H_k[n]^H \right) \Theta [\alpha_k[n]^2],
\]
\[
\xi_k^{NN}[n] = \frac{p_k^L[r_0^2]}{\sigma^2} \left( H_k[n]H_k[n]^H \right) \Theta [\alpha_k[n]^2].\]

To deal with the non-convex constraint (19), we introduce the slack variables \(x = [x_k[n], \forall k, \eta, y = [y_k[n], \forall k, n], \text{and } z = [z_k[n], \forall k, n]\) into the rate function (11). Thus, \(E[R_k[n]]\) can be rewritten as
\[
E[R_k[n]] = \frac{1}{x_k[n]x_k[n] \log_2 \left( 1 + \frac{\xi_k^{LL}[n]}{\alpha_k[n]^2} \right)} + \frac{1}{x_k[n]z_k[n] \log_2 \left( 1 + \frac{\xi_k^{LN}[n]}{\alpha_k[n]^2} \right)} + \frac{1}{z_k[n]x_k[n] \log_2 \left( 1 + \frac{\xi_k^{NL}[n]}{\alpha_k[n]^2} \right)} + \frac{1}{z_k[n]z_k[n] \log_2 \left( 1 + \frac{\xi_k^{NN}[n]}{\alpha_k[n]^2} \right)}.
\]

where
\[
x_k[n] \geq 1 + \frac{\epsilon}{\left( \psi_k[n] - \psi_k[n] - \psi_k[n] - \psi_k[n] \right)} + \frac{\epsilon}{\left( \psi_k[n] - \psi_k[n] - \psi_k[n] - \psi_k[n] \right)} + \frac{\epsilon}{\left( \psi_k[n] - \psi_k[n] - \psi_k[n] - \psi_k[n] \right)} + \frac{\epsilon}{\left( \psi_k[n] - \psi_k[n] - \psi_k[n] - \psi_k[n] \right)}.
\]

Furthermore,
\[
\psi_k[n] \leq \frac{180}{\pi} \arctan \left( \frac{\left( n[k] - n[k] \right)}{\left( n[k] - n[k] \right)} \right),
\]
\[
\phi_k[n] \geq \frac{180}{\pi} \arctan \left( \frac{\left( n[k] - n[k] \right) - \left( n[k] - n[k] \right)}{\left( n[k] - n[k] \right) - \left( n[k] - n[k] \right)} \right).
\]

are the relaxed constraints for the sake of handling the non-affine constraints (5). We can prove by contradiction that constraints (21)-(25) must hold with equalities to ensure that the objective value of problem (18) does not decrease. Note that, after the variable replacement, \(R_k[n]\) in (20) is jointly convex with respect to \(x_k[n], y_k[n], \text{and } z_k[n].\)

Although constraint (24) is non-convex, the right-hand-side (RHS) of (24) is convex with respect to \(\left( n[k] - n[k] \right)\). Since the first-order Taylor approximation of a convex function is a global underestimator, it can be applied at any local points \(\psi_k[n], y_k[n], \text{and } z_k[n]\), and \(\left( n[k] - n[k] \right)\) in the \(l\) th iteration for (20) and (24), i.e., (26), shown at the bottom of the next page, and
\[
\psi_k[n] \leq \frac{180}{\pi} \arctan \left( \frac{\left( n[k] - n[k] \right)}{\left( n[k] - n[k] \right)} \right),
\]
where
\[
B_l[n] = 1 + \frac{\xi_k^{LL}[n]}{\left( y_k[n]^2 \right) \left( y_k[n]^2 \right) \left( y_k[n]^2 \right) \left( y_k[n]^2 \right)} + C_l[n]
\]
\[
= 1 + \frac{\xi_k^{LL}[n]}{\left( y_k[n]^2 \right) \left( y_k[n]^2 \right) \left( y_k[n]^2 \right) \left( y_k[n]^2 \right)} + D_l[n]
\]
\[
= 1 + \frac{\xi_k^{LL}[n]}{\left( y_k[n]^2 \right) \left( y_k[n]^2 \right) \left( y_k[n]^2 \right) \left( y_k[n]^2 \right)} + E_l[n]
\]
\[
= 1 + \frac{\xi_k^{NN}[n]}{\left( y_k[n]^2 \right) \left( y_k[n]^2 \right) \left( y_k[n]^2 \right) \left( y_k[n]^2 \right)} + F_l[n]
\]

Furthermore, \(F_l[n] = \arctan \left( \frac{\left( n[k] - n[k] \right)}{\left( n[k] - n[k] \right)} \right) + G_k[n] = \frac{\left( n[k] - n[k] \right)}{\left( n[k] - n[k] \right)} + H_n^2\).
With (26)-(27), problem (18) can be reformulated into the following convex optimization problem,

$$\max_{Q, \psi_k, \phi_k, z_k, y_k, \eta} \eta$$

s.t. (1) - (2), (21) - (23), (25) - (27),

(28)

where $$\psi_k = \{\psi_k[n], \forall k, n\}$$ and $$\Phi_k = \{\phi_k[n], \forall k, n\}$$. As such, problem (28) can be efficiently solved by CVX [28].

1) UAV Vertical Trajectory Optimization: With the optimal $$A, Q$$, and $$\Theta$$ obtained by problem (12), (17), and (28), the UAV vertical trajectory optimization problem can be reformulated as

$$\max_{H, \psi_k, \eta} \eta$$

s.t. (3), (5), (11b),

(29)

Since problems (18) and (29) are similar in form and differ only slightly in terms of optimization variables $$H$$, the procedure for solving problem (18) can be similarly applied to solve problem (29).

We omit the detailed derivation owing to the page limitation.

2) Overall Algorithm: By applying our proposed problem, (11) can be solved by alternately optimizing variables $$A$$, $$Q$$, and $$H$$, while its solution converges to a preset accuracy $$\epsilon$$, which is summarized in Algorithm 1. Note that the binary solution can be reconstructed with high precision from the obtained continuous variables of GNS transmission scheduling by applying the proposed reconstruction method in [4].

In the following, we discuss the computational complexity of proposed Algorithm 1. Since the four subproblems are solved by applying CVX by the standard interior point method, their computational complexity can be obtained as $$O_1((KN)^{3.5}\log(1/\epsilon))$$, $$O_2(\sqrt{M}\log(1/\epsilon)((KN + 1)M^3 + (KN + 1)^2M^2 + (KN + 1)^3))$$.

Algorithm 1 Proposed Algorithm for Problem (15)

1: Initialization: Initialize $$A^{(0)}, \Theta^{(0)}, Q^{(0)}, H^{(0)}$$ and iteration number $$l = 0$$. Set $$\bar{R}_l^{(0)}$$ and $$\tilde{R}_l^{(0)}$$ by using (10) with given $$A^{(0)}, \Theta^{(0)}, Q^{(0)}, H^{(0)}$$.

2: repeat

3: Solve problem (12) for given $$A^{(l)}, Q^{(l)}, H^{(l)}$$, and denote the optimal solution as $$\bar{A}^{(l+1)}$$.

4: Solve problem (17) for given $$A^{(l)}, Q^{(l)}, H^{(l)}$$, and denote the optimal solution as $$\bar{Q}^{(l+1)}$$.

5: Solve problem (28) for given $$A^{(l)}, Q^{(l)}, H^{(l)}$$, and denote the optimal solution as $$\bar{H}^{(l+1)}$$.

6: Solve problem (29) for given $$A^{(l)}, Q^{(l)}, H^{(l)}$$, and denote the optimal solution as $$\bar{H}^{(l+1)}$$.

7: With given $$\bar{A}^{(l+1)}, \Theta^{(l+1)}, Q^{(l+1)}, H^{(l+1)}$$, update $$\bar{R}_l^{(l+1)}$$ and $$\tilde{R}_l^{(l+1)}$$ by using (10).

8: Update $$l = l + 1$$.

9: until $$\frac{\min(\bar{R}_l^{(l+1)} - \tilde{R}_l^{(l+1)})}{\min(\bar{R}_l^{(l)} - \tilde{R}_l^{(l)})} < \epsilon$$.

IV. SIMULATION RESULTS

In this section, we provide simulation results to show the interesting elevation angle and distance trade-off of the 3D UAV trajectory design under the PLC model (denoted as PLC for brevity). The following schemes are used for comparison: 1) UAV horizontal trajectory design under the PLC scheme with fixed altitude being

$$O_3((2N + 6KN)^{3.5}\log(1/\epsilon))$$, and $$O_4((2N + 6KN)^{3.5}\log(1/\epsilon))$$, respectively. Thus, the total computational complexity of our proposed algorithm is in the order of $$O_1 + O_2 + O_3 + O_4$$.
H = 200 m (denoted as PLCFA); 2) 3D UAV trajectory design under the LC model (denoted as DLC). We assume that GN1 and GN 2 are located at (0, 0, 0) m and (800, 0, 0) m, respectively. Unless otherwise stated, the simulation results are set as: \( v_{\text{max}} = 40 \text{ m/s} \), \( v_{\text{max}} = 20 \text{ m/s} \), \( p_1 = p_2 = 0.1 \text{ W} \), \( \beta_0 = -40 \text{ dB} \), \( H_{\text{min}} = 100 \text{ m} \), \( H_{\text{max}} = 500 \text{ m} \), \( d = \frac{\lambda}{2} \), \( \sigma_z^2 = -169 \text{ dBm} \), \( a = 2.2 \), GN = 3.2, \( a = 11.95 \), and \( b = 0.14 \) [19], [20]. Furthermore, the initialized trajectory of the UAV is set to be a straight-line trajectory with a fixed altitude \( H = 200 \text{ m} \), i.e., the UAV flies from \( q_0 = [-200, -200] \) to \( q_F = [1000, 200] \) at its maximum flying speed.

Fig. 2 shows the different 3D UAV trajectories by three schemes with \( T = 150 \text{ s} \). It can be seen that the UAV in the DLC first descends quickly to \( H_{\text{min}} \), hovers over GN 1, then flies horizontally at its maximum speed, and hovers over GN 2. Finally, the UAV rises and flies back to the final location. This is because hovering above each GN at \( H_{\text{min}} \) suffers from the least path loss for the cascade channel between the UAV and the GNs. By contrast, in the PLC scheme, the UAV first ascends rapidly to increase the elevation angle between the UAV and each GN for a higher LoS probability. Then, the UAV hovers above the midpoint of the two GNs, which results in less path loss while maintaining a larger LoS probability of the cascaded channel. Compared to the PLC scheme that the UAV hovers only above the midpoints of the two GNs, the UAV in the PLCFA scheme hovers close to both sides of the midpoint of the two GNs. This is because that although hovering at the midpoint of the two GNs can maximize the LoS probability of the cascaded channel, i.e., \( P_{\text{LoS}}^{k}[n]P_{\text{LoS}}^{l}[n] \), the larger path loss of the communication links also degrades the rate performance. Therefore, our proposed PLC scheme can take advantage of the additional design brought by the UAV vertical trajectory to obtain a more efficient angle-distance trade-off than the PLCFA scheme.

Fig. 3 illustrates the achieved expected max-min rates of different schemes versus \( T \) when \( M = 100 \). It can be seen that the PLCFA scheme achieves larger rates than the DLC scheme, which indicates the necessity of adopting the more accurate PLC model to describe the LoS/NLoS channel states in the UAV-borne RIS communication system. Furthermore, our proposed PLC scheme significantly improves performance over the PLCFA scheme. The reason is that the additionally designing the UAV vertical trajectory can further increase the LoS probability of the cascaded channel. Fig. 4 shows the achieved expected max-min rates for different schemes with \( T = 150 \text{ s} \) versus different \( M \). As expected, the rate performance is significantly increased when more elements are equipped in the RIS due to the larger passive beamforming gain. In practice, we cannot increase \( M \) indefinitely to obtain higher rates due to the limitation of the size of rotary-wing UAVs. An oversized \( M \) will result in a larger RIS size, which will increase the weight of the UAV and result in greater energy consumption (i.e., shorter endurance). Therefore, an interesting trade-off exists between \( M \) (i.e., related to the RIS size) and the UAV energy consumption for rate improvement.

V. CONCLUSION

This paper investigated the potential of rate enhancement for the aerial RIS-aided communication system under the accurate PLC model in the dense urban environment. The objective was to maximize the minimum average achievable rate. We proposed an efficient iterative algorithm to jointly optimize the communication schedule, the RIS’s phase shift, and the 3D UAV trajectory. Numerical results showed that the proposed scheme has a significant improvement compared to the conventional DLC scheme. Furthermore, our proposed scheme enjoys the additional gain of elevation angle-dependent 3D UAV trajectory design and can effectively balance the elevation angle and distance trade-off between the UAV and the GNs, whereas the DLC scheme cannot. This validates the practical importance of considering the more accurate PLC model to support UAV-borne RIS communications in urban environments.

Note that in the suburban/urban/dense urban environment, the error in the approximated PLC model [26] is extremely small and thus can be ignored. However, this PLC model suffers from errors in the high-rise urban environment, which may cause performance loss. In this case, the hybrid offline-online 3D UAV trajectory design proposed in [17] may be an alternative to better characterize the real-time location-dependent air-ground channel states, which is interesting to study whether the performance loss can be further compensated by employing additional online design.

Although we mainly concentrate on the insightful trade-off between the elevation angle-distance for rate improvement, it is still worthwhile to investigate how to further reduce the complexity of the proposed algorithm by employing some cutting-edge methods, such as deep reinforcement learning (DRL) [29].

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